

# **Yosys Manual**

**Clifford Wolf**

# Abstract

Most of today's digital design is done in HDL code (mostly Verilog or VHDL) and with the help of HDL synthesis tools.

In special cases such as synthesis for coarse-grain cell libraries or when testing new synthesis algorithms it might be necessary to write a custom HDL synthesis tool or add new features to an existing one. In these cases the availability of a Free and Open Source (FOSS) synthesis tool that can be used as basis for custom tools would be helpful.

In the absence of such a tool, the Yosys Open SYnthesis Suite (Yosys) was developed. This document covers the design and implementation of this tool. At the moment the main focus of Yosys lies on the high-level aspects of digital synthesis. The pre-existing FOSS logic-synthesis tool ABC is used by Yosys to perform advanced gate-level optimizations.

An evaluation of Yosys based on real-world designs is included. It is shown that Yosys can be used as-is to synthesize such designs. The results produced by Yosys in this tests were successfully verified using formal verification and are comparable in quality to the results produced by a commercial synthesis tool.

This document was originally published as bachelor thesis at the Vienna University of Technology [[Wol13](#)].

# Abbreviations

AIG	And-Inverter-Graph
ASIC	Application-Specific Integrated Circuit
AST	Abstract Syntax Tree
BDD	Binary Decision Diagram
BLIF	Berkeley Logic Interchange Format
EDA	Electronic Design Automation
EDIF	Electronic Design Interchange Format
ER Diagram	Entity-Relationship Diagram
FOSS	Free and Open-Source Software
FPGA	Field-Programmable Gate Array
FSM	Finite-state machine
HDL	Hardware Description Language
LPM	Library of Parameterized Modules
RTLIL	RTL Intermediate Language
RTL	Register Transfer Level
SAT	Satisfiability Problem
VHDL	VHSIC Hardware Description Language
VHSIC	Very-High-Speed Integrated Circuit
YOSYS	Yosys Open SYnthesis Suite

# Contents

<b>1</b>	<b>Introduction</b>	<b>14</b>
1.1	History of Yosys	14
1.2	Structure of this Document	15
<b>2</b>	<b>Basic Principles</b>	<b>16</b>
2.1	Levels of Abstraction	16
2.1.1	System Level	17
2.1.2	High Level	17
2.1.3	Behavioural Level	17
2.1.4	Register-Transfer Level (RTL)	18
2.1.5	Logical Gate Level	18
2.1.6	Physical Gate Level	19
2.1.7	Switch Level	19
2.1.8	Yosys	19
2.2	Features of Synthesizable Verilog	19
2.2.1	Structural Verilog	19
2.2.2	Expressions in Verilog	20
2.2.3	Behavioural Modelling	20
2.2.4	Functions and Tasks	21
2.2.5	Conditionals, Loops and Generate-Statements	21
2.2.6	Arrays and Memories	21
2.3	Challenges in Digital Circuit Synthesis	22
2.3.1	Standards Compliance	22
2.3.2	Optimizations	23
2.3.3	Technology Mapping	23
2.4	Script-Based Synthesis Flows	23
2.5	Methods from Compiler Design	24
2.5.1	Lexing and Parsing	24
2.5.2	Multi-Pass Compilation	25

## CONTENTS

<b>3</b>	<b>Approach</b>	<b>27</b>
3.1	Data- and Control-Flow	27
3.2	Internal Formats in Yosys	28
3.3	Typical Use Case	28
<b>4</b>	<b>Implementation Overview</b>	<b>30</b>
4.1	Simplified Data Flow	30
4.2	The RTL Intermediate Language	31
4.2.1	RTLIL Identifiers	32
4.2.2	RTLIL::Design and RTLIL::Module	33
4.2.3	RTLIL::Cell and RTLIL::Wire	33
4.2.4	RTLIL::SigSpec	34
4.2.5	RTLIL::Process	35
4.2.6	RTLIL::Memory	37
4.3	Command Interface and Synthesis Scripts	37
4.4	Source Tree and Build System	38
<b>5</b>	<b>Internal Cell Library</b>	<b>39</b>
5.1	RTL Cells	39
5.1.1	Unary Operators	39
5.1.2	Binary Operators	40
5.1.3	Multiplexers	41
5.1.4	Registers	42
5.1.5	Memories	43
5.1.6	Finite State Machines	46
5.1.7	Specify rules	46
5.1.8	Formal verification cells	46
5.2	Gates	46
<b>6</b>	<b>Programming Yosys Extensions</b>	<b>53</b>
6.1	The “CodingReadme” File	53
6.2	The “stubsnet” Example Module	58

## CONTENTS

<b>7</b>	<b>The Verilog and AST Frontends</b>	<b>62</b>
7.1	Transforming Verilog to AST . . . . .	62
7.1.1	The Verilog Preprocessor . . . . .	63
7.1.2	The Verilog Lexer . . . . .	63
7.1.3	The Verilog Parser . . . . .	63
7.2	Transforming AST to RTLIL . . . . .	64
7.2.1	AST Simplification . . . . .	64
7.2.2	Generating RTLIL . . . . .	66
7.3	Synthesizing Verilog always Blocks . . . . .	66
7.3.1	The ProcessGenerator Algorithm . . . . .	68
7.3.2	The proc pass . . . . .	71
7.4	Synthesizing Verilog Arrays . . . . .	72
7.5	Synthesizing Parametric Designs . . . . .	72
<b>8</b>	<b>Optimizations</b>	<b>73</b>
8.1	Simple Optimizations . . . . .	73
8.1.1	The opt_expr pass . . . . .	73
8.1.2	The opt_muxtree pass . . . . .	74
8.1.3	The opt_reduce pass . . . . .	74
8.1.4	The opt_rmdff pass . . . . .	75
8.1.5	The opt_clean pass . . . . .	75
8.1.6	The opt_merge pass . . . . .	75
8.2	FSM Extraction and Encoding . . . . .	75
8.2.1	FSM Detection . . . . .	76
8.2.2	FSM Extraction . . . . .	76
8.2.3	FSM Optimization . . . . .	77
8.2.4	FSM Recoding . . . . .	78
8.3	Logic Optimization . . . . .	78
<b>9</b>	<b>Technology Mapping</b>	<b>79</b>
9.1	Cell Substitution . . . . .	79
9.2	Subcircuit Substitution . . . . .	79
9.3	Gate-Level Technology Mapping . . . . .	80
<b>A</b>	<b>Auxiliary Libraries</b>	<b>81</b>
A.1	SHA1 . . . . .	81
A.2	BigInt . . . . .	81
A.3	SubCircuit . . . . .	81
A.4	ezSAT . . . . .	81

## CONTENTS

<b>B</b>	<b>Auxiliary Programs</b>	<b>82</b>
B.1	yosys-config . . . . .	82
B.2	yosys-filterlib . . . . .	82
B.3	yosys-abc . . . . .	82
<b>C</b>	<b>Command Reference Manual</b>	<b>83</b>
C.1	abc – use ABC for technology mapping . . . . .	83
C.2	abc9 – use ABC9 for technology mapping . . . . .	86
C.3	abc9_exe – use ABC9 for technology mapping . . . . .	88
C.4	abc9_ops – helper functions for ABC9 . . . . .	90
C.5	add – add objects to the design . . . . .	91
C.6	aigmap – map logic to and-inverter-graph circuit . . . . .	91
C.7	alumacc – extract ALU and MACC cells . . . . .	91
C.8	anlogic_eqn – Anlogic: Calculate equations for luts . . . . .	92
C.9	anlogic_fixcarry – Anlogic: fix carry chain . . . . .	92
C.10	assertpmux – adds asserts for parallel muxes . . . . .	92
C.11	async2sync – convert async FF inputs to sync circuits . . . . .	92
C.12	attrmap – renaming attributes . . . . .	93
C.13	attrmvcp – move or copy attributes from wires to driving cells . . . . .	93
C.14	autoname – automatically assign names to objects . . . . .	94
C.15	blackbox – convert modules into blackbox modules . . . . .	94
C.16	bugpoint – minimize testcases . . . . .	94
C.17	cd – a shortcut for 'select -module <name>' . . . . .	95
C.18	check – check for obvious problems in the design . . . . .	95
C.19	chformal – change formal constraints of the design . . . . .	96
C.20	chparam – re-evaluate modules with new parameters . . . . .	97
C.21	chtype – change type of cells in the design . . . . .	97
C.22	clean – remove unused cells and wires . . . . .	97
C.23	clk2fflogic – convert clocked FFs to generic \$ff cells . . . . .	98
C.24	clkbufmap – insert global buffers on clock networks . . . . .	98
C.25	connect – create or remove connections . . . . .	98
C.26	connect_rpc – connect to RPC frontend . . . . .	99
C.27	connwrappers – match width of input-output port pairs . . . . .	100
C.28	coolrunner2_fixup – insert necessary buffer cells for CoolRunner-II architecture . . . . .	100
C.29	coolrunner2_sop – break \$sop cells into ANDTERM/ORTERM cells . . . . .	100
C.30	copy – copy modules in the design . . . . .	100
C.31	cover – print code coverage counters . . . . .	101

## CONTENTS

C.32	cutpoint – adds formal cut points to the design . . . . .	101
C.33	debug – run command with debug log messages enabled . . . . .	102
C.34	delete – delete objects in the design . . . . .	102
C.35	deminout – demote inout ports to input or output . . . . .	102
C.36	design – save, restore and reset current design . . . . .	102
C.37	determine_init – Determine the init value of cells . . . . .	103
C.38	dff2dffe – transform \$dff cells to \$dffe cells . . . . .	104
C.39	dff2dffs – process sync set/reset with SR over CE priority . . . . .	104
C.40	dffinit – set INIT param on FF cells . . . . .	104
C.41	dfflibmap – technology mapping of flip-flops . . . . .	105
C.42	dump – print parts of the design in ilang format . . . . .	105
C.43	echo – turning echoing back of commands on and off . . . . .	106
C.44	ecp5_ffinit – ECP5: handle FF init values . . . . .	106
C.45	ecp5_gsr – ECP5: handle GSR . . . . .	106
C.46	edgetypes – list all types of edges in selection . . . . .	106
C.47	efinix_fixcarry – Efinix: fix carry chain . . . . .	107
C.48	efinix_gbuf – Efinix: insert global clock buffers . . . . .	107
C.49	equiv_add – add a \$equiv cell . . . . .	107
C.50	equiv_induct – proving \$equiv cells using temporal induction . . . . .	107
C.51	equiv_make – prepare a circuit for equivalence checking . . . . .	108
C.52	equiv_mark – mark equivalence checking regions . . . . .	108
C.53	equiv_miter – extract miter from equiv circuit . . . . .	108
C.54	equiv_opt – prove equivalence for optimized circuit . . . . .	109
C.55	equiv_purge – purge equivalence checking module . . . . .	110
C.56	equiv_remove – remove \$equiv cells . . . . .	110
C.57	equiv_simple – try proving simple \$equiv instances . . . . .	110
C.58	equiv_status – print status of equivalent checking module . . . . .	111
C.59	equiv_struct – structural equivalence checking . . . . .	111
C.60	eval – evaluate the circuit given an input . . . . .	111
C.61	exec – execute commands in the operating system shell . . . . .	112
C.62	expose – convert internal signals to module ports . . . . .	112
C.63	extract – find subcircuits and replace them with cells . . . . .	113
C.64	extract_counter – Extract GreenPak4 counter cells . . . . .	115
C.65	extract_fa – find and extract full/half adders . . . . .	115
C.66	extract_reduce – converts gate chains into \$reduce_* cells . . . . .	116
C.67	extractinv – extract explicit inverter cells for invertible cell pins . . . . .	116



## CONTENTS

C.68	flatten – flatten design	116
C.69	flowmap – pack LUTs with FlowMap	117
C.70	fmcombine – combine two instances of a cell into one	117
C.71	fminit – set init values/sequences for formal	118
C.72	freduce – perform functional reduction	118
C.73	fsm – extract and optimize finite state machines	119
C.74	fsm_detect – finding FSMs in design	120
C.75	fsm_expand – expand FSM cells by merging logic into it	120
C.76	fsm_export – exporting FSMs to KISS2 files	120
C.77	fsm_extract – extracting FSMs in design	121
C.78	fsm_info – print information on finite state machines	121
C.79	fsm_map – mapping FSMs to basic logic	121
C.80	fsm_opt – optimize finite state machines	121
C.81	fsm_recode – recoding finite state machines	121
C.82	greenpak4_dffinv – merge greenpak4 inverters and DFF/latches	122
C.83	help – display help messages	122
C.84	hierarchy – check, expand and clean up design hierarchy	122
C.85	hilomap – technology mapping of constant hi- and/or lo-drivers	124
C.86	history – show last interactive commands	124
C.87	ice40_braminit – iCE40: perform SB_RAM40_4K initialization from file	124
C.88	ice40_dsp – iCE40: map multipliers	124
C.89	ice40_ffinit – iCE40: handle FF init values	125
C.90	ice40_ffssr – iCE40: merge synchronous set/reset into FF cells	125
C.91	ice40_opt – iCE40: perform simple optimizations	125
C.92	ice40_wrapcarry – iCE40: wrap carries	125
C.93	insbuf – insert buffer cells for connected wires	126
C.94	iopadmap – technology mapping of i/o pads (or buffers)	126
C.95	json – write design in JSON format	127
C.96	log – print text and log files	127
C.97	logger – set logger properties	128
C.98	ls – list modules or objects in modules	128
C.99	ltp – print longest topological path	129
C.100	lut2mux – convert \$lut to \$_MUX_	129
C.101	maccmap – mapping macc cells	129
C.102	memory – translate memories to basic cells	129
C.103	memory_bram – map memories to block rams	130

## CONTENTS

C.104memory_collect – creating multi-port memory cells . . . . .	131
C.105memory_dff – merge input/output DFFs into memories . . . . .	132
C.106memory_map – translate multiport memories to basic cells . . . . .	132
C.107memory_memx – emulate vlog sim behavior for mem ports . . . . .	132
C.108memory_nordff – extract read port FFs from memories . . . . .	132
C.109memory_share – consolidate memory ports . . . . .	133
C.110memory_unpack – unpack multi-port memory cells . . . . .	133
C.111miter – automatically create a miter circuit . . . . .	133
C.112mutate – generate or apply design mutations . . . . .	134
C.113muxcover – cover trees of MUX cells with wider MUXes . . . . .	135
C.114muxpack – \$mux/\$pmux cascades to \$pmux . . . . .	136
C.115nlutmap – map to LUTs of different sizes . . . . .	136
C.116onehot – optimize \$eq cells for onehot signals . . . . .	136
C.117opt – perform simple optimizations . . . . .	137
C.118opt_clean – remove unused cells and wires . . . . .	137
C.119opt_demorgan – Optimize reductions with DeMorgan equivalents . . . . .	137
C.120opt_expr – perform const folding and simple expression rewriting . . . . .	138
C.121opt_lut – optimize LUT cells . . . . .	138
C.122opt_lut_ins – discard unused LUT inputs . . . . .	139
C.123opt_mem – optimize memories . . . . .	139
C.124opt_merge – consolidate identical cells . . . . .	139
C.125opt_muxtree – eliminate dead trees in multiplexer trees . . . . .	139
C.126opt_reduce – simplify large MUXes and AND/OR gates . . . . .	140
C.127opt_rmdff – remove DFFs with constant inputs . . . . .	140
C.128opt_share – merge mutually exclusive cells of the same type that share an input signal . . . . .	140
C.129paramap – renaming cell parameters . . . . .	140
C.130peepopt – collection of peephole optimizers . . . . .	141
C.131plugin – load and list loaded plugins . . . . .	141
C.132pmux2shiftx – transform \$pmux cells to \$shiftx cells . . . . .	141
C.133pmuxtree – transform \$pmux cells to trees of \$mux cells . . . . .	142
C.134portlist – list (top-level) ports . . . . .	142
C.135prep – generic synthesis script . . . . .	142
C.136proc – translate processes to netlists . . . . .	144
C.137proc_arst – detect asynchronous resets . . . . .	144
C.138proc_clean – remove empty parts of processes . . . . .	145
C.139proc_dff – extract flip-flops from processes . . . . .	145

## CONTENTS

C.140proc_dlatch – extract latches from processes . . . . .	145
C.141proc_init – convert initial block to init attributes . . . . .	145
C.142proc_mux – convert decision trees to multiplexers . . . . .	145
C.143proc_prune – remove redundant assignments . . . . .	146
C.144proc_rmdead – eliminate dead trees in decision trees . . . . .	146
C.145qwp – quadratic wirelength placer . . . . .	146
C.146read – load HDL designs . . . . .	146
C.147read_aiger – read AIGER file . . . . .	147
C.148read_blif – read BLIF file . . . . .	148
C.149read_ilang – read modules from ilang file . . . . .	148
C.150read_json – read JSON file . . . . .	148
C.151read_liberty – read cells from liberty file . . . . .	148
C.152read_verilog – read modules from Verilog file . . . . .	149
C.153rename – rename object in the design . . . . .	152
C.154rmports – remove module ports with no connections . . . . .	153
C.155sat – solve a SAT problem in the circuit . . . . .	153
C.156scatter – add additional intermediate nets . . . . .	156
C.157scc – detect strongly connected components (logic loops) . . . . .	156
C.158scratchpad – get/set values in the scratchpad . . . . .	157
C.159script – execute commands from file or wire . . . . .	158
C.160select – modify and view the list of selected objects . . . . .	158
C.161setattr – set/unset attributes on objects . . . . .	162
C.162setparam – set/unset parameters on objects . . . . .	163
C.163setundef – replace undef values with defined constants . . . . .	163
C.164sf2_jobs – SF2: insert IO buffers . . . . .	163
C.165share – perform sat-based resource sharing . . . . .	164
C.166shell – enter interactive command mode . . . . .	164
C.167show – generate schematics using graphviz . . . . .	165
C.168shregmap – map shift registers . . . . .	166
C.169sim – simulate the circuit . . . . .	168
C.170simplemap – mapping simple coarse-grain cells . . . . .	168
C.171splice – create explicit splicing cells . . . . .	169
C.172splitnets – split up multi-bit nets . . . . .	169
C.173stat – print some statistics . . . . .	170
C.174submod – moving part of a module to a new submodule . . . . .	170
C.175supercover – add hi/lo cover cells for each wire bit . . . . .	171

## CONTENTS

C.176synth – generic synthesis script . . . . .	171
C.177synth_achronix – synthesis for Achronix Speedster22i FPGAs. . . . .	173
C.178synth_anlogic – synthesis for Anlogic FPGAs . . . . .	174
C.179synth_coolrunner2 – synthesis for Xilinx Coolrunner-II CPLDs . . . . .	176
C.180synth_easic – synthesis for eASIC platform . . . . .	177
C.181synth_ecp5 – synthesis for ECP5 FPGAs . . . . .	178
C.182synth_efinix – synthesis for Efinix FPGAs . . . . .	181
C.183synth_gowin – synthesis for Gowin FPGAs . . . . .	183
C.184synth_greenpak4 – synthesis for GreenPAK4 FPGAs . . . . .	185
C.185synth_ice40 – synthesis for iCE40 FPGAs . . . . .	187
C.186synth_intel – synthesis for Intel (Altera) FPGAs. . . . .	190
C.187synth_sf2 – synthesis for SmartFusion2 and IGLOO2 FPGAs . . . . .	192
C.188synth_xilinx – synthesis for Xilinx FPGAs . . . . .	194
C.189tcl – execute a TCL script file . . . . .	197
C.190techmap – generic technology mapper . . . . .	198
C.191tee – redirect command output to file . . . . .	201
C.192test_abcloop – automatically test handling of loops in abc command . . . . .	201
C.193test_autotb – generate simple test benches . . . . .	201
C.194test_cell – automatically test the implementation of a cell type . . . . .	202
C.195test_pmgcn – test pass for pmgcn . . . . .	203
C.196torder – print cells in topological order . . . . .	203
C.197trace – redirect command output to file . . . . .	204
C.198tribuf – infer tri-state buffers . . . . .	204
C.199uniquify – create unique copies of modules . . . . .	204
C.200verific – load Verilog and VHDL designs using Verific . . . . .	204
C.201verilog_defaults – set default options for read_verilog . . . . .	207
C.202verilog_defines – define and undefine verilog defines . . . . .	207
C.203wbflip – flip the whitebox attribute . . . . .	208
C.204wreduce – reduce the word size of operations if possible . . . . .	208
C.205write_aiger – write design to AIGER file . . . . .	208
C.206write_blif – write design to BLIF file . . . . .	209
C.207write_btor – write design to BTOR file . . . . .	210
C.208write_cxxrtl – convert design to C++ RTL simulation . . . . .	211
C.209write_edif – write design to EDIF netlist file . . . . .	211
C.210write_file – write a text to a file . . . . .	212
C.211write_firrtl – write design to a FIRRTL file . . . . .	212

## CONTENTS

C.212	write_ilang – write design to ilang file . . . . .	213
C.213	write_intersynth – write design to InterSynth netlist file . . . . .	213
C.214	write_json – write design to a JSON file . . . . .	213
C.215	write_simplec – convert design to simple C code . . . . .	217
C.216	write_smt2 – write design to SMT-LIBv2 file . . . . .	217
C.217	write_smv – write design to SMV file . . . . .	220
C.218	write_spice – write design to SPICE netlist file . . . . .	221
C.219	write_table – write design as connectivity table . . . . .	221
C.220	write_verilog – write design to Verilog file . . . . .	221
C.221	write_xaiger – write design to XAIGER file . . . . .	223
C.222	xilinx_dffopt – Xilinx: optimize FF control signal usage . . . . .	223
C.223	xilinx_dsp – Xilinx: pack resources into DSPs . . . . .	224
C.224	xilinx_srl – Xilinx shift register extraction . . . . .	224
C.225	zinit – add inverters so all FF are zero-initialized . . . . .	225
<b>D</b>	<b>RTLIL Text Representation . . . . .</b>	<b>226</b>
D.1	Lexical elements . . . . .	226
D.1.1	Characters . . . . .	226
D.1.2	Identifiers . . . . .	226
D.1.3	Values . . . . .	227
D.1.4	Strings . . . . .	227
D.1.5	Comments . . . . .	227
D.2	File . . . . .	228
D.2.1	Autoindex statements . . . . .	228
D.2.2	Modules . . . . .	228
D.2.3	Attribute statements . . . . .	228
D.2.4	Signal specifications . . . . .	229
D.2.5	Connections . . . . .	229
D.2.6	Wires . . . . .	229
D.2.7	Memories . . . . .	230
D.2.8	Cells . . . . .	230
D.2.9	Processes . . . . .	230
D.2.10	Switches . . . . .	231
D.2.11	Syncs . . . . .	231
<b>E</b>	<b>Application Notes . . . . .</b>	<b>232</b>

# Chapter 1

## Introduction

This document presents the Free and Open Source (FOSS) Verilog HDL synthesis tool “Yosys”. Its design and implementation as well as its performance on real-world designs is discussed in this document.

### 1.1 History of Yosys

A Hardware Description Language (HDL) is a computer language used to describe circuits. A HDL synthesis tool is a computer program that takes a formal description of a circuit written in an HDL as input and generates a netlist that implements the given circuit as output.

Currently the most widely used and supported HDLs for digital circuits are Verilog [Ver06][Ver02] and VHDL<sup>1</sup> [VHD09][VHD04]. Both HDLs are used for test and verification purposes as well as logic synthesis, resulting in a set of synthesizable and a set of non-synthesizable language features. In this document we only look at the synthesizable subset of the language features.

In recent work on heterogeneous coarse-grain reconfigurable logic [WGS<sup>+</sup>12] the need for a custom application-specific HDL synthesis tool emerged. It was soon realised that a synthesis tool that understood Verilog or VHDL would be preferred over a synthesis tool for a custom HDL. Given an existing Verilog or VHDL front end, the work for writing the necessary additional features and integrating them in an existing tool can be estimated to be about the same as writing a new tool with support for a minimalistic custom HDL.

The proposed custom HDL synthesis tool should be licensed under a Free and Open Source Software (FOSS) licence. So an existing FOSS Verilog or VHDL synthesis tool would have been needed as basis to build upon. The main advantages of choosing Verilog or VHDL is the ability to synthesize existing HDL code and to mitigate the requirement for circuit-designers to learn a new language. In order to take full advantage of any existing FOSS Verilog or VHDL tool, such a tool would have to provide a feature-complete implementation of the synthesizable HDL subset.

Basic RTL synthesis is a well understood field [HS96]. Lexing, parsing and processing of computer languages [ASU86] is a thoroughly researched field. All the information required to write such tools has been openly available for a long time, and it is therefore likely that a FOSS HDL synthesis tool with a feature-complete Verilog or VHDL front end must exist which can be used as a basis for a custom RTL synthesis tool.

Due to the author’s preference for Verilog over VHDL it was decided early on to go for Verilog instead of VHDL<sup>2</sup>. So the existing FOSS Verilog synthesis tools were evaluated (see App. ??). The results of this evaluation are utterly devastating. Therefore a completely new Verilog synthesis tool was implemented and is recommended as basis for custom synthesis tools. This is the tool that is discussed in this document.

---

<sup>1</sup>VHDL is an acronym for “VHSIC hardware description language” and VHSIC is an acronym for “Very-High-Speed Integrated Circuits”.

<sup>2</sup>A quick investigation into FOSS VHDL tools yielded similar grim results for FOSS VHDL synthesis tools.

## 1.2 Structure of this Document

The structure of this document is as follows:

Chapter 1 is this introduction.

Chapter 2 covers a short introduction to the world of HDL synthesis. Basic principles and the terminology are outlined in this chapter.

Chapter 3 gives the quickest possible outline to how the problem of implementing a HDL synthesis tool is approached in the case of Yosys.

Chapter 4 contains a more detailed overview of the implementation of Yosys. This chapter covers the data structures used in Yosys to represent a design in detail and is therefore recommended reading for everyone who is interested in understanding the Yosys internals.

Chapter 5 covers the internal cell library used by Yosys. This is especially important knowledge for anyone who wants to understand the intermediate netlists used internally by Yosys.

Chapter 6 gives a tour to the internal APIs of Yosys. This is recommended reading for everyone who actually wants to read or write Yosys source code. The chapter concludes with an example loadable module for Yosys.

Chapters 7, 8, and 9 cover three important pieces of the synthesis pipeline: The Verilog frontend, the optimization passes and the technology mapping to the target architecture, respectively.

Chapter ?? covers the evaluation of the performance (correctness and quality) of Yosys on real-world input data. The chapter concludes the main part of this document with conclusions and outlook to future work.

Various appendices, including a command reference manual (App. C) and an evaluation of pre-existing FOSS Verilog synthesis tools (App. ??) complete this document.

# Chapter 2

## Basic Principles

This chapter contains a short introduction to the basic principles of digital circuit synthesis.

### 2.1 Levels of Abstraction

Digital circuits can be represented at different levels of abstraction. During the design process a circuit is usually first specified using a higher level abstraction. Implementation can then be understood as finding a functionally equivalent representation at a lower abstraction level. When this is done automatically using software, the term *synthesis* is used.

So synthesis is the automatic conversion of a high-level representation of a circuit to a functionally equivalent low-level representation of a circuit. Figure 2.1 lists the different levels of abstraction and how they relate to different kinds of synthesis.

Regardless of the way a lower level representation of a circuit is obtained (synthesis or manual design), the lower level representation is usually verified by comparing simulation results of the lower level and the higher level representation<sup>1</sup>. Therefore even if no synthesis is used, there must still be a simulatable representation of the circuit in all levels to allow for verification of the design.

<sup>1</sup>In recent years formal equivalence checking also became an important verification method for validating RTL and lower abstraction representation of the design.

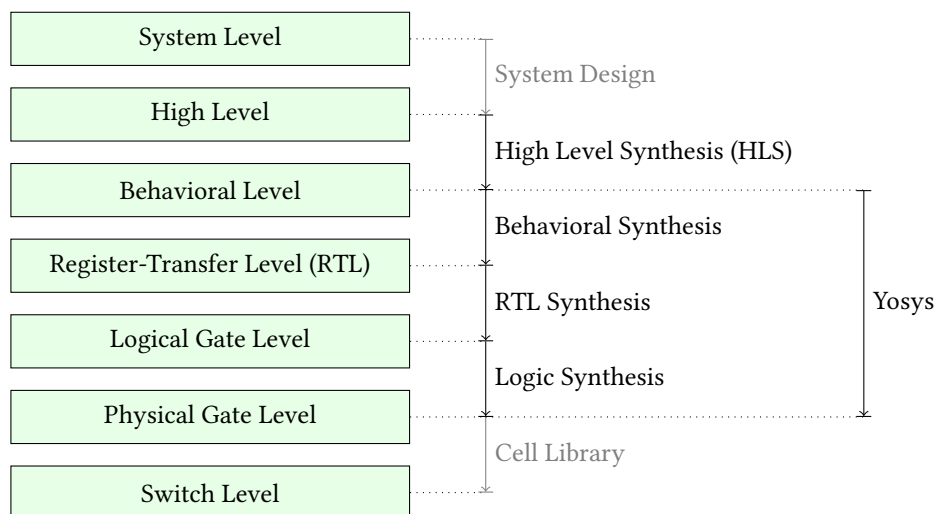


Figure 2.1: Different levels of abstraction and synthesis.



Note: The exact meaning of terminology such as “High-Level” is of course not fixed over time. For example the HDL “ABEL” was first introduced in 1985 as “A High-Level Design Language for Programmable Logic Devices” [LHBB85], but would not be considered a “High-Level Language” today.

### 2.1.1 System Level

The System Level abstraction of a system only looks at its biggest building blocks like CPUs and computing cores. At this level the circuit is usually described using traditional programming languages like C/C++ or Matlab. Sometimes special software libraries are used that are aimed at simulation circuits on the system level, such as SystemC.

Usually no synthesis tools are used to automatically transform a system level representation of a circuit to a lower-level representation. But system level design tools exist that can be used to connect system level building blocks.

The IEEE 1685-2009 standard defines the IP-XACT file format that can be used to represent designs on the system level and building blocks that can be used in such system level designs. [IP-10]

### 2.1.2 High Level

The high-level abstraction of a system (sometimes referred to as *algorithmic* level) is also often represented using traditional programming languages, but with a reduced feature set. For example when representing a design at the high level abstraction in C, pointers can only be used to mimic concepts that can be found in hardware, such as memory interfaces. Full featured dynamic memory management is not allowed as it has no corresponding concept in digital circuits.

Tools exist to synthesize high level code (usually in the form of C/C++/SystemC code with additional metadata) to behavioural HDL code (usually in the form of Verilog or VHDL code). Aside from the many commercial tools for high level synthesis there are also a number of FOSS tools for high level synthesis [16] [19].

### 2.1.3 Behavioural Level

At the behavioural abstraction level a language aimed at hardware description such as Verilog or VHDL is used to describe the circuit, but so-called *behavioural modelling* is used in at least part of the circuit description. In behavioural modelling there must be a language feature that allows for imperative programming to be used to describe data paths and registers. This is the `always`-block in Verilog and the `process`-block in VHDL.

In behavioural modelling, code fragments are provided together with a *sensitivity list*; a list of signals and conditions. In simulation, the code fragment is executed whenever a signal in the sensitivity list changes its value or a condition in the sensitivity list is triggered. A synthesis tool must be able to transfer this representation into an appropriate datapath followed by the appropriate types of register.

For example consider the following Verilog code fragment:

```
1 always @(posedge clk)
2     y <= a + b;
```

In simulation the statement `y <= a + b` is executed whenever a positive edge on the signal `clk` is detected. The synthesis result however will contain an adder that calculates the sum `a + b` all the time, followed by a d-type flip-flop with the adder output on its D-input and the signal `y` on its Q-output.

Usually the imperative code fragments used in behavioural modelling can contain statements for conditional execution (**if**- and **case**-statements in Verilog) as well as loops, as long as those loops can be completely unrolled.

Interestingly there seems to be no other FOSS Tool that is capable of performing Verilog or VHDL behavioural syntheses besides Yosys (see App. ??).

### 2.1.4 Register-Transfer Level (RTL)

On the Register-Transfer Level the design is represented by combinatorial data paths and registers (usually d-type flip flops). The following Verilog code fragment is equivalent to the previous Verilog example, but is in RTL representation:

```

1 assign tmp = a + b;           // combinatorial data path
2
3 always @(posedge clk)        // register
4     y <= tmp;
```

A design in RTL representation is usually stored using HDLs like Verilog and VHDL. But only a very limited subset of features is used, namely minimalistic `always`-blocks (Verilog) or `process`-blocks (VHDL) that model the register type used and unconditional assignments for the datapath logic. The use of HDLs on this level simplifies simulation as no additional tools are required to simulate a design in RTL representation.

Many optimizations and analyses can be performed best at the RTL level. Examples include FSM detection and optimization, identification of memories or other larger building blocks and identification of shareable resources.

Note that RTL is the first abstraction level in which the circuit is represented as a graph of circuit elements (registers and combinatorial cells) and signals. Such a graph, when encoded as list of cells and connections, is called a netlist.

RTL synthesis is easy as each circuit node element in the netlist can simply be replaced with an equivalent gate-level circuit. However, usually the term *RTL synthesis* does not only refer to synthesizing an RTL netlist to a gate level netlist but also to performing a number of highly sophisticated optimizations within the RTL representation, such as the examples listed above.

A number of FOSS tools exist that can perform isolated tasks within the domain of RTL synthesis steps. But there seems to be no FOSS tool that covers a wide range of RTL synthesis operations.

### 2.1.5 Logical Gate Level

At the logical gate level the design is represented by a netlist that uses only cells from a small number of single-bit cells, such as basic logic gates (AND, OR, NOT, XOR, etc.) and registers (usually D-Type Flip-flops).

A number of netlist formats exists that can be used on this level, e.g. the Electronic Design Interchange Format (EDIF), but for ease of simulation often a HDL netlist is used. The latter is a HDL file (Verilog or VHDL) that only uses the most basic language constructs for instantiation and connecting of cells.

There are two challenges in logic synthesis: First finding opportunities for optimizations within the gate level netlist and second the optimal (or at least good) mapping of the logic gate netlist to an equivalent netlist of physically available gate types.

The simplest approach to logic synthesis is *two-level logic synthesis*, where a logic function is converted into a sum-of-products representation, e.g. using a Karnaugh map. This is a simple approach, but has exponential worst-case effort and cannot make efficient use of physical gates other than AND/NAND-, OR/NOR- and NOT-Gates.

Therefore modern logic synthesis tools utilize much more complicated *multi-level logic synthesis* algorithms [BHSV90]. Most of these algorithms convert the logic function to a Binary-Decision-Diagram (BDD) or And-Inverter-Graph (AIG) and work from that representation. The former has the advantage that it has a unique normalized form. The latter has much better worst case performance and is therefore better suited for the synthesis of large logic functions.

Good FOSS tools exist for multi-level logic synthesis [27] [26] [28].

Yosys contains basic logic synthesis functionality but can also use ABC [27] for the logic synthesis step. Using ABC is recommended.

### 2.1.6 Physical Gate Level

On the physical gate level only gates are used that are physically available on the target architecture. In some cases this may only be NAND, NOR and NOT gates as well as D-Type registers. In other cases this might include cells that are more complex than the cells used at the logical gate level (e.g. complete half-adders). In the case of an FPGA-based design the physical gate level representation is a netlist of LUTs with optional output registers, as these are the basic building blocks of FPGA logic cells.

For the synthesis tool chain this abstraction is usually the lowest level. In case of an ASIC-based design the cell library might contain further information on how the physical cells map to individual switches (transistors).

### 2.1.7 Switch Level

A switch level representation of a circuit is a netlist utilizing single transistors as cells. Switch level modelling is possible in Verilog and VHDL, but is seldom used in modern designs, as in modern digital ASIC or FPGA flows the physical gates are considered the atomic build blocks of the logic circuit.

### 2.1.8 Yosys

Yosys is a Verilog HDL synthesis tool. This means that it takes a behavioural design description as input and generates an RTL, logical gate or physical gate level description of the design as output. Yosys' main strengths are behavioural and RTL synthesis. A wide range of commands (synthesis passes) exist within Yosys that can be used to perform a wide range of synthesis tasks within the domain of behavioural, rtl and logic synthesis. Yosys is designed to be extensible and therefore is a good basis for implementing custom synthesis tools for specialised tasks.

## 2.2 Features of Synthesizable Verilog

The subset of Verilog [Ver06] that is synthesizable is specified in a separate IEEE standards document, the IEEE standard 1364.1-2002 [Ver02]. This standard also describes how certain language constructs are to be interpreted in the scope of synthesis.

This section provides a quick overview of the most important features of synthesizable Verilog, structured in order of increasing complexity.

### 2.2.1 Structural Verilog

*Structural Verilog* (also known as *Verilog Netlists*) is a Netlist in Verilog syntax. Only the following language constructs are used in this case:

- Constant values
- Wire and port declarations
- Static assignments of signals to other signals
- Cell instantiations

Many tools (especially at the back end of the synthesis chain) only support structural Verilog as input. ABC is an example of such a tool. Unfortunately there is no standard specifying what *Structural Verilog* actually is, leading to some confusion about what syntax constructs are supported in structural Verilog when it comes to features such as attributes or multi-bit signals.

## 2.2.2 Expressions in Verilog

In all situations where Verilog accepts a constant value or signal name, expressions using arithmetic operations such as +, - and \*, boolean operations such as & (AND), | (OR) and ^ (XOR) and many others (comparison operations, unary operator, etc.) can also be used.

During synthesis these operators are replaced by cells that implement the respective function.

Many FOSS tools that claim to be able to process Verilog in fact only support basic structural Verilog and simple expressions. Yosys can be used to convert full featured synthesizable Verilog to this simpler subset, thus enabling such applications to be used with a richer set of Verilog features.

## 2.2.3 Behavioural Modelling

Code that utilizes the Verilog `always` statement is using *Behavioural Modelling*. In behavioural modelling, a circuit is described by means of imperative program code that is executed on certain events, namely any change, a rising edge, or a falling edge of a signal. This is a very flexible construct during simulation but is only synthesizable when one of the following is modelled:

- **Asynchronous or latched logic**

In this case the sensitivity list must contain all expressions that are used within the `always` block. The syntax `@*` can be used for these cases. Examples of this kind include:

```

1 // asynchronous
2 always @* begin
3     if (add_mode)
4         y <= a + b;
5     else
6         y <= a - b;
7 end
8
9 // latched
10 always @* begin
11     if (!hold)
12         y <= a + b;
13 end

```

Note that latched logic is often considered bad style and in many cases just the result of sloppy HDL design. Therefore many synthesis tools generate warnings whenever latched logic is generated.

- **Synchronous logic (with optional synchronous reset)**

This is logic with d-type flip-flops on the output. In this case the sensitivity list must only contain the respective clock edge. Example:

```

1 // counter with synchronous reset
2 always @(posedge clk) begin
3     if (reset)
4         y <= 0;
5     else
6         y <= y + 1;
7 end

```

- **Synchronous logic with asynchronous reset**

This is logic with d-type flip-flops with asynchronous resets on the output. In this case the sensitivity list must only contain the respective clock and reset edges. The values assigned in the reset branch must be constant. Example:

```

1 // counter with asynchronous reset
2 always @(posedge clk, posedge reset) begin
3     if (reset)
4         y <= 0;
5     else
6         y <= y + 1;
7 end

```

Many synthesis tools support a wider subset of flip-flops that can be modelled using `always`-statements (including Yosys). But only the ones listed above are covered by the Verilog synthesis standard and when writing new designs one should limit herself or himself to these cases.

In behavioural modelling, blocking assignments (`=`) and non-blocking assignments (`<=`) can be used. The concept of blocking vs. non-blocking assignment is one of the most misunderstood constructs in Verilog [CI00].

The blocking assignment behaves exactly like an assignment in any imperative programming language, while with the non-blocking assignment the right hand side of the assignment is evaluated immediately but the actual update of the left hand side register is delayed until the end of the time-step. For example the Verilog code `a <= b; b <= a;` exchanges the values of the two registers. See Sec. ?? for a more detailed description of this behaviour.

#### 2.2.4 Functions and Tasks

Verilog supports *Functions* and *Tasks* to bundle statements that are used in multiple places (similar to *Procedures* in imperative programming). Both constructs can be implemented easily by substituting the function/task-call with the body of the function or task.

#### 2.2.5 Conditionals, Loops and Generate-Statements

Verilog supports **if-else**-statements and **for**-loops inside **always**-statements.

It also supports both features in **generate**-statements on the module level. This can be used to selectively enable or disable parts of the module based on the module parameters (**if-else**) or to generate a set of similar subcircuits (**for**).

While the **if-else**-statement inside an `always`-block is part of behavioural modelling, the three other cases are (at least for a synthesis tool) part of a built-in macro processor. Therefore it must be possible for the synthesis tool to completely unroll all loops and evaluate the condition in all **if-else**-statement in **generate**-statements using const-folding.

Examples for this can be found in Fig. ?? and Fig. ?? in App. ??.

#### 2.2.6 Arrays and Memories

Verilog supports arrays. This is in general a synthesizable language feature. In most cases arrays can be synthesized by generating addressable memories. However, when complex or asynchronous access patterns are used, it is not possible to model an array as memory. In these cases the array must be modelled using individual signals for each word and all accesses to the array must be implemented using large multiplexers.

In some cases it would be possible to model an array using memories, but it is not desired. Consider the following delay circuit:

```

1 module (clk, in_data, out_data);
2
3 parameter BITS = 8;
4 parameter STAGES = 4;
5
6 input clk;
7 input [BITS-1:0] in_data;
8 output [BITS-1:0] out_data;
9 reg [BITS-1:0] ffs [STAGES-1:0];
10
11 integer i;
12 always @(posedge clk) begin
13     ffs[0] <= in_data;
14     for (i = 1; i < STAGES; i = i+1)
15         ffs[i] <= ffs[i-1];
16 end
17
18 assign out_data = ffs[STAGES-1];
19
20 endmodule

```

This could be implemented using an addressable memory with STAGES input and output ports. A better implementation would be to use a simple chain of flip-flops (a so-called shift register). This better implementation can either be obtained by first creating a memory-based implementation and then optimizing it based on the static address signals for all ports or directly identifying such situations in the language front end and converting all memory accesses to direct accesses to the correct signals.

## 2.3 Challenges in Digital Circuit Synthesis

This section summarizes the most important challenges in digital circuit synthesis. Tools can be characterized by how well they address these topics.

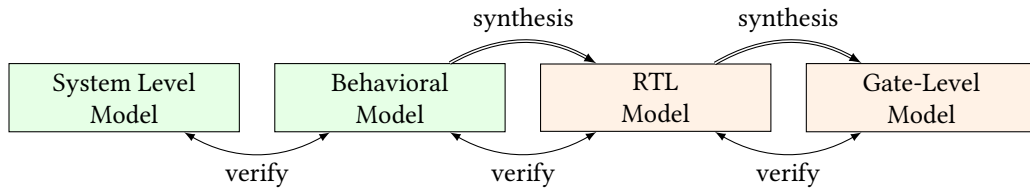
### 2.3.1 Standards Compliance

The most important challenge is compliance with the HDL standards in question (in case of Verilog the IEEE Standards 1364.1-2002 and 1364-2005). This can be broken down in two items:

- Completeness of implementation of the standard
- Correctness of implementation of the standard

Completeness is mostly important to guarantee compatibility with existing HDL code. Once a design has been verified and tested, HDL designers are very reluctant regarding changes to the design, even if it is only about a few minor changes to work around a missing feature in a new synthesis tool.

Correctness is crucial. In some areas this is obvious (such as correct synthesis of basic behavioural models). But it is also crucial for the areas that concern minor details of the standard, such as the exact rules for handling signed expressions, even when the HDL code does not target different synthesis tools. This is because (unlike software source code that is only processed by compilers), in most design flows HDL code is not only processed by the synthesis tool but also by one or more simulators and sometimes even a formal verification tool. It is key for this verification process that all these tools use the same interpretation for the HDL code.



**Figure 2.2:** Typical design flow. Green boxes represent manually created models. Orange boxes represent models generated by synthesis tools.

### 2.3.2 Optimizations

Generally it is hard to give a one-dimensional description of how well a synthesis tool optimizes the design. First of all because not all optimizations are applicable to all designs and all synthesis tasks. Some optimizations work (best) on a coarse-grained level (with complex cells such as adders or multipliers) and others work (best) on a fine-grained level (single bit gates). Some optimizations target area and others target speed. Some work well on large designs while others don't scale well and can only be applied to small designs.

A good tool is capable of applying a wide range of optimizations at different levels of abstraction and gives the designer control over which optimizations are performed (or skipped) and what the optimization goals are.

### 2.3.3 Technology Mapping

Technology mapping is the process of converting the design into a netlist of cells that are available in the target architecture. In an ASIC flow this might be the process-specific cell library provided by the fab. In an FPGA flow this might be LUT cells as well as special function units such as dedicated multipliers. In a coarse-grain flow this might even be more complex special function units.

An open and vendor independent tool is especially of interest if it supports a wide range of different types of target architectures.

## 2.4 Script-Based Synthesis Flows

A digital design is usually started by implementing a high-level or system-level simulation of the desired function. This description is then manually transformed (or re-implemented) into a synthesizable lower-level description (usually at the behavioural level) and the equivalence of the two representations is verified by simulating both and comparing the simulation results.

Then the synthesizable description is transformed to lower-level representations using a series of tools and the results are again verified using simulation. This process is illustrated in Fig. 2.2.

In this example the System Level Model and the Behavioural Model are both manually written design files. After the equivalence of system level model and behavioural model has been verified, the lower level representations of the design can be generated using synthesis tools. Finally the RTL Model and the Gate-Level Model are verified and the design process is finished.

However, in any real-world design effort there will be multiple iterations for this design process. The reason for this can be the late change of a design requirement or the fact that the analysis of a low-abstraction model (e.g. gate-level timing analysis) revealed that a design change is required in order to meet the design requirements (e.g. maximum possible clock speed).

Whenever the behavioural model or the system level model is changed their equivalence must be re-verified by re-running the simulations and comparing the results. Whenever the behavioural model is changed the synthesis must be re-run and the synthesis results must be re-verified.

Token-Type	Token-Value
TOK_ASSIGN	-
TOK_IDENTIFIER	"foo"
TOK_EQ	-
TOK_IDENTIFIER	"bar"
TOK_PLUS	-
TOK_NUMBER	42
TOK_SEMICOLON	-

**Table 2.1:** Exemplary token list for the statement **"assign foo = bar + 42;"**.

In order to guarantee reproducibility it is important to be able to re-run all automatic steps in a design project with a fixed set of settings easily. Because of this, usually all programs used in a synthesis flow can be controlled using scripts. This means that all functions are available via text commands. When such a tool provides a GUI, this is complementary to, and not instead of, a command line interface.

Usually a synthesis flow in an UNIX/Linux environment would be controlled by a shell script that calls all required tools (synthesis and simulation/verification in this example) in the correct order. Each of these tools would be called with a script file containing commands for the respective tool. All settings required for the tool would be provided by these script files so that no manual interaction would be necessary. These script files are considered design sources and should be kept under version control just like the source code of the system level and the behavioural model.

## 2.5 Methods from Compiler Design

Some parts of synthesis tools involve problem domains that are traditionally known from compiler design. This section addresses some of these domains.

### 2.5.1 Lexing and Parsing

The best known concepts from compiler design are probably *lexing* and *parsing*. These are two methods that together can be used to process complex computer languages easily. [ASU86]

A *lexer* consumes single characters from the input and generates a stream of *lexical tokens* that consist of a *type* and a *value*. For example the Verilog input **"assign foo = bar + 42;"** might be translated by the lexer to the list of lexical tokens given in Tab. 2.1.

The lexer is usually generated by a lexer generator (e.g. `flex` [17]) from a description file that is using regular expressions to specify the text pattern that should match the individual tokens.

The lexer is also responsible for skipping ignored characters (such as whitespace outside string constants and comments in the case of Verilog) and converting the original text snippet to a token value.

Note that individual keywords use different token types (instead of a keyword type with different token values). This is because the parser usually can only use the Token-Type to make a decision on the grammatical role of a token.

The parser then transforms the list of tokens into a parse tree that closely resembles the productions from the computer languages grammar. As the lexer, the parser is also typically generated by a code generator (e.g. `bison` [18]) from a grammar description in Backus-Naur Form (BNF).

Let's consider the following BNF (in Bison syntax):

```

1 assign_stmt: TOK_ASSIGN TOK_IDENTIFIER TOK_EQ expr TOK_SEMICOLON;
2 expr: TOK_IDENTIFIER | TOK_NUMBER | expr TOK_PLUS expr;
```



The parser converts the token list to the parse tree in Fig. 2.3. Note that the parse tree never actually exists as a whole as data structure in memory. Instead the parser calls user-specified code snippets (so-called *reduce-functions*) for all inner nodes of the parse tree in depth-first order.

In some very simple applications (e.g. code generation for stack machines) it is possible to perform the task at hand directly in the reduce functions. But usually the reduce functions are only used to build an in-memory data structure with the relevant information from the parse tree. This data structure is called an *abstract syntax tree* (AST).

The exact format for the abstract syntax tree is application specific (while the format of the parse tree and token list are mostly dictated by the grammar of the language at hand). Figure 2.4 illustrates what an AST for the parse tree in Fig. 2.3 could look like.

Usually the AST is then converted into yet another representation that is more suitable for further processing. In compilers this is often an assembler-like three-address-code intermediate representation. [ASU86]

## 2.5.2 Multi-Pass Compilation

Complex problems are often best solved when split up into smaller problems. This is certainly true for compilers as well as for synthesis tools. The components responsible for solving the smaller problems can be connected in two different ways: through *Single-Pass Pipelining* and by using *Multiple Passes*.

Traditionally a parser and lexer are connected using the pipelined approach: The lexer provides a function that is called by the parser. This function reads data from the input until a complete lexical token has been read. Then this token is returned to the parser. So the lexer does not first generate a complete list of lexical tokens and then pass it to the parser. Instead they run concurrently and the parser can consume tokens as the lexer produces them.

The single-pass pipelining approach has the advantage of lower memory footprint (at no time must the complete design be kept in memory) but has the disadvantage of tighter coupling between the interacting components.

Therefore single-pass pipelining should only be used when the lower memory footprint is required or the components are also conceptually tightly coupled. The latter certainly is the case for a parser and its lexer. But when data is passed between two conceptually loosely coupled components it is often beneficial to use a multi-pass approach.

In the multi-pass approach the first component processes all the data and the result is stored in a in-memory data structure. Then the second component is called with this data. This reduces complexity, as only one component is running at a time. It also improves flexibility as components can be exchanged easier.

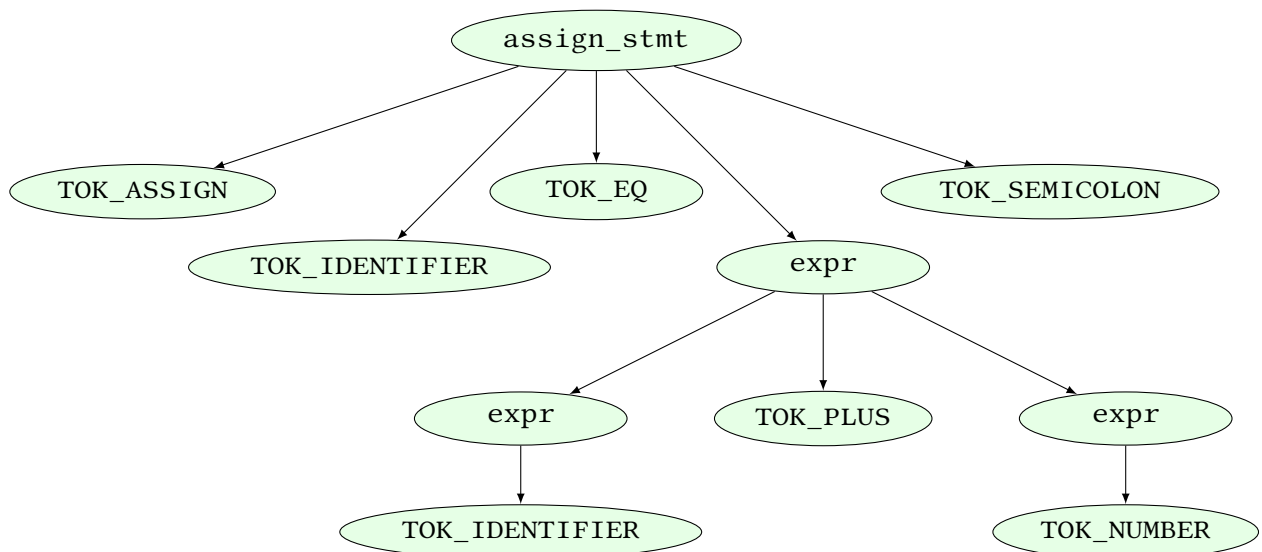
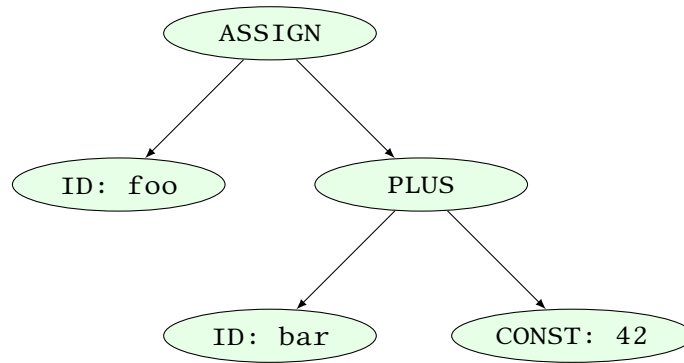


Figure 2.3: Example parse tree for the Verilog expression “**assign** foo = bar + 42;”.



**Figure 2.4:** Example abstract syntax tree for the Verilog expression “**assign** foo = bar + 42;”.

Most modern compilers are multi-pass compilers.

## Chapter 3

# Approach

Yosys is a tool for synthesising (behavioural) Verilog HDL code to target architecture netlists. Yosys aims at a wide range of application domains and thus must be flexible and easy to adapt to new tasks. This chapter covers the general approach followed in the effort to implement this tool.

### 3.1 Data- and Control-Flow

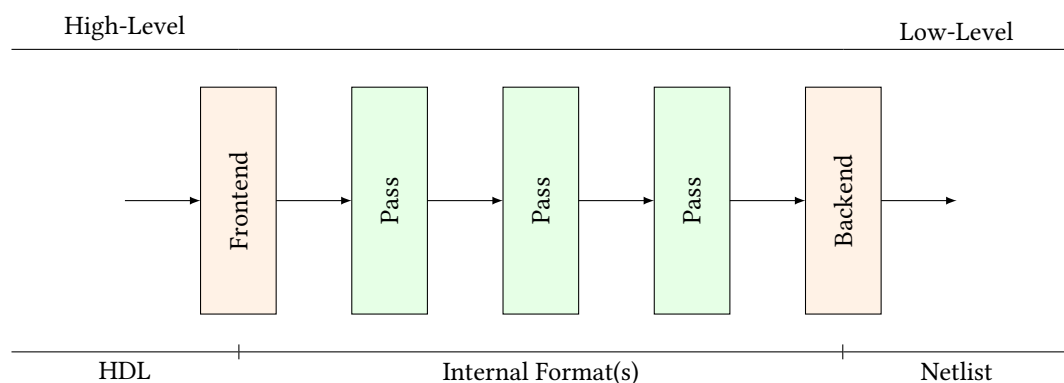
The data- and control-flow of a typical synthesis tool is very similar to the data- and control-flow of a typical compiler: different subsystems are called in a predetermined order, each consuming the data generated by the last subsystem and generating the data for the next subsystem (see Fig. 3.1).

The first subsystem to be called is usually called a *frontend*. It does not process the data generated by another subsystem but instead reads the user input—in the case of a HDL synthesis tool, the behavioural HDL code.

The subsystems that consume data from previous subsystems and produce data for the next subsystems (usually in the same or a similar format) are called *passes*.

The last subsystem that is executed transforms the data generated by the last pass into a suitable output format and writes it to a disk file. This subsystem is usually called the *backend*.

In Yosys all frontends, passes and backends are directly available as commands in the synthesis script. Thus the user can easily create a custom synthesis flow just by calling passes in the right order in a synthesis script.



**Figure 3.1:** General data- and control-flow of a synthesis tool

## 3.2 Internal Formats in Yosys

Yosys uses two different internal formats. The first is used to store an abstract syntax tree (AST) of a Verilog input file. This format is simply called *AST* and is generated by the Verilog Frontend. This data structure is consumed by a subsystem called *AST Frontend*<sup>1</sup>. This AST Frontend then generates a design in Yosys' main internal format, the Register-Transfer-Level-Intermediate-Language (RTLIL) representation. It does that by first performing a number of simplifications within the AST representation and then generating RTLIL from the simplified AST data structure.

The RTLIL representation is used by all passes as input and outputs. This has the following advantages over using different representational formats between different passes:

- The passes can be rearranged in a different order and passes can be removed or inserted.
- Passes can simply pass-thru the parts of the design they don't change without the need to convert between formats. In fact Yosys passes output the same data structure they received as input and performs all changes in place.
- All passes use the same interface, thus reducing the effort required to understand a pass when reading the Yosys source code, e.g. when adding additional features.

The RTLIL representation is basically a netlist representation with the following additional features:

- An internal cell library with fixed-function cells to represent RTL datapath and register cells as well as logical gate-level cells (single-bit gates and registers).
- Support for multi-bit values that can use individual bits from wires as well as constant bits to represent coarse-grain netlists.
- Support for basic behavioural constructs (if-then-else structures and multi-case switches with a sensitivity list for updating the outputs).
- Support for multi-port memories.

The use of RTLIL also has the disadvantage of having a very powerful format between all passes, even when doing gate-level synthesis where the more advanced features are not needed. In order to reduce complexity for passes that operate on a low-level representation, these passes check the features used in the input RTLIL and fail to run when unsupported high-level constructs are used. In such cases a pass that transforms the higher-level constructs to lower-level constructs must be called from the synthesis script first.

## 3.3 Typical Use Case

The following example script may be used in a synthesis flow to convert the behavioural Verilog code from the input file `design.v` to a gate-level netlist `synth.v` using the cell library described by the Liberty file [25] `cells.lib`:

```

1 # read input file to internal representation
2 read_verilog design.v
3
4 # convert high-level behavioral parts ("processes") to d-type flip-flops and muxes
5 proc
6
7 # perform some simple optimizations

```

<sup>1</sup>In Yosys the term *pass* is only used to refer to commands that operate on the RTLIL data structure.

```
8  opt
9
10 # convert high-level memory constructs to d-type flip-flops and multiplexers
11 memory
12
13 # perform some simple optimizations
14 opt
15
16 # convert design to (logical) gate-level netlists
17 techmap
18
19 # perform some simple optimizations
20 opt
21
22 # map internal register types to the ones from the cell library
23 dfflibmap -liberty cells.lib
24
25 # use ABC to map remaining logic to cells from the cell library
26 abc -liberty cells.lib
27
28 # cleanup
29 opt
30
31 # write results to output file
32 write_verilog synth.v
```

A detailed description of the commands available in Yosys can be found in App. [C](#).

## Chapter 4

# Implementation Overview

Yosys is an extensible open source hardware synthesis tool. It is aimed at designers who are looking for an easily accessible, universal, and vendor-independent synthesis tool, as well as scientists who do research in electronic design automation (EDA) and are looking for an open synthesis framework that can be used to test algorithms on complex real-world designs.

Yosys can synthesize a large subset of Verilog 2005 and has been tested with a wide range of real-world designs, including the OpenRISC 1200 CPU [23], the openMSP430 CPU [22], the OpenCores I<sup>2</sup>C master [20] and the k68 CPU [21].

As of this writing a Yosys VHDL frontend is in development.

Yosys is written in C++ (using some features from the new C++11 standard). This chapter describes some of the fundamental Yosys data structures. For the sake of simplicity the C++ type names used in the Yosys implementation are used in this chapter, even though the chapter only explains the conceptual idea behind it and can be used as reference to implement a similar system in any language.

### 4.1 Simplified Data Flow

Figure 4.1 shows the simplified data flow within Yosys. Rectangles in the figure represent program modules and ellipses internal data structures that are used to exchange design data between the program modules.

Design data is read in using one of the frontend modules. The high-level HDL frontends for Verilog and VHDL code generate an abstract syntax tree (AST) that is then passed to the AST frontend. Note that both HDL frontends use the same AST representation that is powerful enough to cover the Verilog HDL and VHDL language.

The AST Frontend then compiles the AST to Yosys's main internal data format, the RTL Intermediate Language (RTLIL). A more detailed description of this format is given in the next section.

There is also a text representation of the RTLIL data structure that can be parsed using the RTLIL Frontend.

The design data may then be transformed using a series of passes that all operate on the RTLIL representation of the design.

Finally the design in RTLIL representation is converted back to text by one of the backends, namely the Verilog Backend for generating Verilog netlists and the RTLIL Backend for writing the RTLIL data in the same format that is understood by the RTLIL Frontend.

With the exception of the AST Frontend, which is called by the high-level HDL frontends and can't be called directly by the user, all program modules are called by the user (usually using a synthesis script that contains text commands for Yosys).

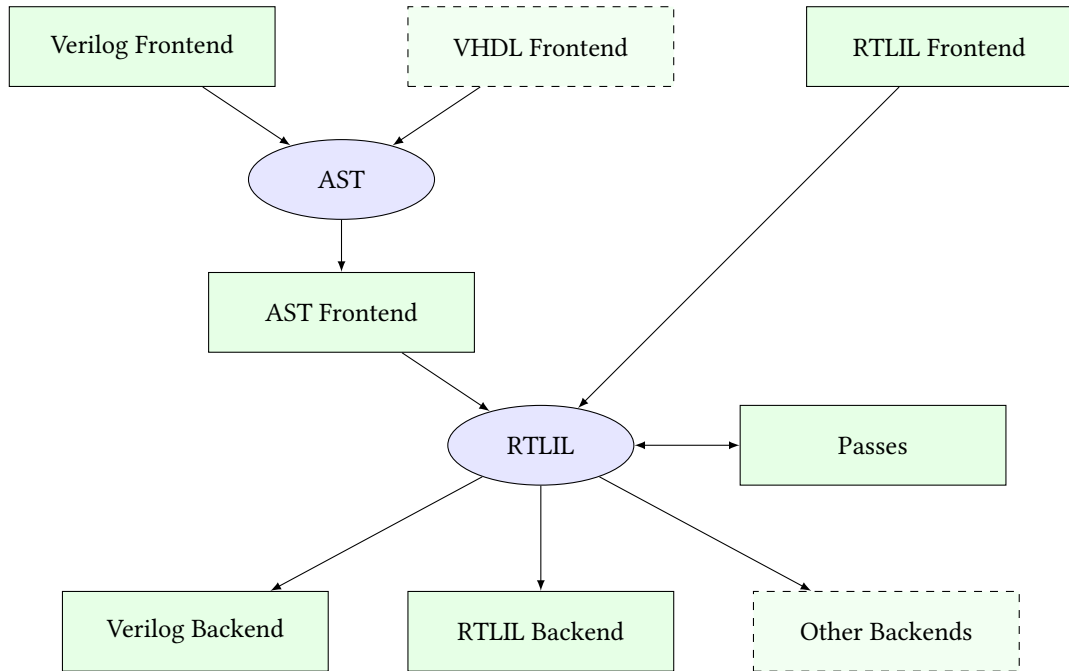


Figure 4.1: Yosys simplified data flow (ellipses: data structures, rectangles: program modules)

By combining passes in different ways and/or adding additional passes to Yosys it is possible to adapt Yosys to a wide range of applications. For this to be possible it is key that (1) all passes operate on the same data structure (RTLIL) and (2) that this data structure is powerful enough to represent the design in different stages of the synthesis.

## 4.2 The RTL Intermediate Language

All frontends, passes and backends in Yosys operate on a design in RTLIL representation. The only exception are the high-level frontends that use the AST representation as an intermediate step before generating RTLIL data.

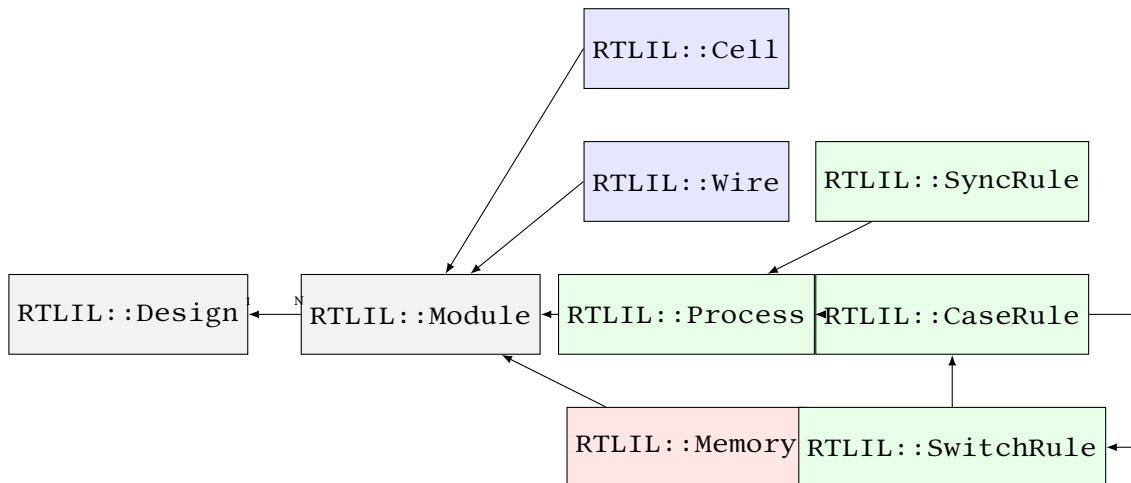
In order to avoid reinventing names for the RTLIL classes, they are simply referred to by their full C++ name, i.e. including the `RTLIL::` namespace prefix, in this document.

Figure 4.2 shows a simplified Entity-Relationship Diagram (ER Diagram) of RTLIL. In  $1 : N$  relationships the arrow points from the  $N$  side to the 1. For example one `RTLIL::Design` contains  $N$  (zero to many) instances of `RTLIL::Module`. A two-pointed arrow indicates a  $1 : 1$  relationship.

The `RTLIL::Design` is the root object of the RTLIL data structure. There is always one “current design” in memory which passes operate on, frontends add data to and backends convert to exportable formats. But in some cases passes internally generate additional `RTLIL::Design` objects. For example when a pass is reading an auxiliary Verilog file such as a cell library, it might create an additional `RTLIL::Design` object and call the Verilog frontend with this other object to parse the cell library.

There is only one active `RTLIL::Design` object that is used by all frontends, passes and backends called by the user, e.g. using a synthesis script. The `RTLIL::Design` then contains zero to many `RTLIL::Module` objects. This corresponds to modules in Verilog or entities in VHDL. Each module in turn contains objects from three different categories:

- `RTLIL::Cell` and `RTLIL::Wire` objects represent classical netlist data.



**Figure 4.2:** Simplified RTLIL Entity-Relationship Diagram

- RTLIL::Process objects represent the decision trees (if-then-else statements, etc.) and synchronization declarations (clock signals and sensitivity) from Verilog always and VHDL process blocks.
- RTLIL::Memory objects represent addressable memories (arrays).

Usually the output of the synthesis procedure is a netlist, i.e. all RTLIL::Process and RTLIL::Memory objects must be replaced by RTLIL::Cell and RTLIL::Wire objects by synthesis passes.

All features of the HDL that cannot be mapped directly to these RTLIL classes must be transformed to an RTLIL-compatible representation by the HDL frontend. This includes Verilog-features such as generate-blocks, loops and parameters.

The following sections contain a more detailed description of the different parts of RTLIL and rationale behind some of the design decisions.

### 4.2.1 RTLIL Identifiers

All identifiers in RTLIL (such as module names, port names, signal names, cell types, etc.) follow the following naming convention: they must either start with a backslash (\) or a dollar sign (\$).

Identifiers starting with a backslash are public visible identifiers. Usually they originate from one of the HDL input files. For example the signal name “\sig42” is most likely a signal that was declared using the name “sig42” in an HDL input file. On the other hand the signal name “\$sig42” is an auto-generated signal name. The backends convert all identifiers that start with a dollar sign to identifiers that do not collide with identifiers that start with a backslash.

This has three advantages:

- First, it is impossible that an auto-generated identifier collides with an identifier that was provided by the user.
- Second, the information about which identifiers were originally provided by the user is always available which can help guide some optimizations. For example the “opt\_rmunused” tries to preserve signals with a user-provided name but doesn’t hesitate to delete signals that have auto-generated names when they just duplicate other signals.



- Third, the delicate job of finding suitable auto-generated public visible names is deferred to one central location. Internally auto-generated names that may hold important information for Yosys developers can be used without disturbing external tools. For example the Verilog backend assigns names in the form `_integer_`.

Whitespace and control characters (any character with an ASCII code 32 or less) are not allowed in RTLIL identifiers; most frontends and backends cannot support these characters in identifiers.

In order to avoid programming errors, the RTLIL data structures check if all identifiers start with either a backslash or a dollar sign, and contain no whitespace or control characters. Violating these rules results in a runtime error.

All RTLIL identifiers are case sensitive.

Some transformations, such as flattening, may have to change identifiers provided by the user to avoid name collisions. When that happens, attribute `hdlname` is attached to the object with the changed identifier. This attribute contains one name (if emitted directly by the frontend, or is a result of disambiguation) or multiple names separated by spaces (if a result of flattening). All names specified in the `hdlname` attribute are public and do not include the leading ```.

## 4.2.2 RTLIL::Design and RTLIL::Module

The RTLIL::Design object is basically just a container for RTLIL::Module objects. In addition to a list of RTLIL::Module objects the RTLIL::Design also keeps a list of *selected objects*, i.e. the objects that passes should operate on. In most cases the whole design is selected and therefore passes operate on the whole design. But this mechanism can be useful for more complex synthesis jobs in which only parts of the design should be affected by certain passes.

Besides the objects shown in the ER diagram in Fig. 4.2 an RTLIL::Module object contains the following additional properties:

- The module name
- A list of attributes
- A list of connections between wires
- An optional frontend callback used to derive parametrized variations of the module

The attributes can be Verilog attributes imported by the Verilog frontend or attributes assigned by passes. They can be used to store additional metadata about modules or just mark them to be used by certain part of the synthesis script but not by others.

Verilog and VHDL both support parametric modules (known as “generic entities” in VHDL). The RTLIL format does not support parametric modules itself. Instead each module contains a callback function into the AST frontend to generate a parametrized variation of the RTLIL::Module as needed. This callback then returns the auto-generated name of the parametrized variation of the module. (A hash over the parameters and the module name is used to prohibit the same parametrized variation from being generated twice. For modules with only a few parameters, a name directly containing all parameters is generated instead of a hash string.)

## 4.2.3 RTLIL::Cell and RTLIL::Wire

A module contains zero to many RTLIL::Cell and RTLIL::Wire objects. Objects of these types are used to model netlists. Usually the goal of all synthesis efforts is to convert all modules to a state where the functionality of the module is implemented only by cells from a given cell library and wires to connect these cells with each other. Note that module ports are just wires with a special property.

An RTLIL::Wire object has the following properties:

- The wire name
- A list of attributes
- A width (buses are just wires with a width > 1)
- Bus direction (MSB to LSB or vice versa)
- Lowest valid bit index (LSB or MSB depending on bus direction)
- If the wire is a port: port number and direction (input/output/inout)

As with modules, the attributes can be Verilog attributes imported by the Verilog frontend or attributes assigned by passes.

In Yosys, busses (signal vectors) are represented using a single wire object with a width > 1. So Yosys does not convert signal vectors to individual signals. This makes some aspects of RTLIL more complex but enables Yosys to be used for coarse grain synthesis where the cells of the target architecture operate on entire signal vectors instead of single bit wires.

In Verilog and VHDL, busses may have arbitrary bounds, and LSB can have either the lowest or the highest bit index. In RTLIL, bit 0 always corresponds to LSB; however, information from the HDL frontend is preserved so that the bus will be correctly indexed in error messages, backend output, constraint files, etc.

An RTLIL::Cell object has the following properties:

- The cell name and type
- A list of attributes
- A list of parameters (for parametric cells)
- Cell ports and the connections of ports to wires and constants

The connections of ports to wires are coded by assigning an RTLIL::SigSpec to each cell port. The RTLIL::SigSpec data type is described in the next section.

#### 4.2.4 RTLIL::SigSpec

A “signal” is everything that can be applied to a cell port. I.e.

- Any constant value of arbitrary bit-width  
For example: 1337, 16'b0000010100111001, 1'b1, 1'bx
- All bits of a wire or a selection of bits from a wire  
For example: mywire, mywire[24], mywire[15:8]
- Concatenations of the above  
For example: {16'd1337, mywire[15:8]}

The RTLIL::SigSpec data type is used to represent signals. The RTLIL::Cell object contains one RTLIL::SigSpec for each cell port.

In addition, connections between wires are represented using a pair of RTLIL::SigSpec objects. Such pairs are needed in different locations. Therefore the type name RTLIL::SigSig was defined for such a pair.

### 4.2.5 RTLIL::Process

When a high-level HDL frontend processes behavioural code it splits it up into data path logic (e.g. the expression  $a + b$  is replaced by the output of an adder that takes  $a$  and  $b$  as inputs) and an RTLIL::Process that models the control logic of the behavioural code. Let's consider a simple example:

```

1 module ff_with_en_and_async_reset(clock, reset, enable, d, q);
2   input clock, reset, enable, d;
3   output reg q;
4   always @(posedge clock, posedge reset)
5       if (reset)
6           q <= 0;
7       else if (enable)
8           q <= d;
9 endmodule

```

In this example there is no data path and therefore the RTLIL::Module generated by the frontend only contains a few RTLIL::Wire objects and an RTLIL::Process. The RTLIL::Process in RTLIL syntax:

```

1 process $proc$ff_with_en_and_async_reset.v:4$1
2     assign $0\q[0:0] \q
3     switch \reset
4         case 1'1
5             assign $0\q[0:0] 1'0
6         case
7             switch \enable
8                 case 1'1
9                     assign $0\q[0:0] \d
10                case
11                    end
12            end
13    sync posedge \clock
14        update \q $0\q[0:0]
15    sync posedge \reset
16        update \q $0\q[0:0]
17 end

```

This RTLIL::Process contains two RTLIL::SyncRule objects, two RTLIL::SwitchRule objects and five RTLIL::CaseRule objects. The wire  $\$0\backslash q[0:0]$  is an automatically created wire that holds the next value of  $\backslash q$ . The lines 2...12 describe how  $\$0\backslash q[0:0]$  should be calculated. The lines 13...16 describe how the value of  $\$0\backslash q[0:0]$  is used to update  $\backslash q$ .

An RTLIL::Process is a container for zero or more RTLIL::SyncRule objects and exactly one RTLIL::CaseRule object, which is called the *root case*.

An RTLIL::SyncRule object contains an (optional) synchronization condition (signal and edge-type) and zero or more assignments (RTLIL::SigSig). The `always` synchronization condition is used to break combinatorial loops when a latch should be inferred instead.

An RTLIL::CaseRule is a container for zero or more assignments (RTLIL::SigSig) and zero or more RTLIL::SwitchRule objects. An RTLIL::SwitchRule objects is a container for zero or more RTLIL::CaseRule objects.

In the above example the lines 2...12 are the root case. Here  $\$0\backslash q[0:0]$  is first assigned the old value  $\backslash q$  as default value (line 2). The root case also contains an RTLIL::SwitchRule object (lines 3...12). Such an object is very similar to the C `switch` statement as it uses a control signal ( $\backslash reset$  in this case) to determine which of its cases should be active. The RTLIL::SwitchRule object then contains one RTLIL::CaseRule object per case. In

this example there is a case<sup>1</sup> for `\reset == 1` that causes `$0\q[0:0]` to be set (lines 4 and 5) and a default case that in turn contains a switch that sets `$0\q[0:0]` to the value of `\d` if `\enable` is active (lines 6...11).

A case can specify zero or more compare values that will determine whether it matches. Each of the compare values must be the exact same width as the control signal. When more than one compare value is specified, the case matches if any of them matches the control signal; when zero compare values are specified, the case always matches (i.e. it is the default case).

A switch prioritizes cases from first to last: multiple cases can match, but only the first matched case becomes active. This normally synthesizes to a priority encoder. The `parallel_case` attribute allows passes to assume that no more than one case will match, and `full_case` attribute allows passes to assume that exactly one case will match; if these invariants are ever dynamically violated, the behavior is undefined. These attributes are useful when an invariant invisible to the synthesizer causes the control signal to never take certain bit patterns.

The lines 13...16 then cause `\q` to be updated whenever there is a positive clock edge on `\clock` or `\reset`.

In order to generate such a representation, the language frontend must be able to handle blocking and nonblocking assignments correctly. However, the language frontend does not need to identify the correct type of storage element for the output signal or generate multiplexers for the decision tree. This is done by passes that work on the RTLIL representation. Therefore it is relatively easy to substitute these steps with other algorithms that target different target architectures or perform optimizations or other transformations on the decision trees before further processing them.

One of the first actions performed on a design in RTLIL representation in most synthesis scripts is identifying asynchronous resets. This is usually done using the `proc_arst` pass. This pass transforms the above example to the following RTLIL::Process:

```

1 process $proc$ff_with_en_and_async_reset.v:4$1
2     assign $0\q[0:0] \q
3     switch \enable
4         case 1'1
5             assign $0\q[0:0] \d
6         case
7     end
8     sync posedge \clock
9         update \q $0\q[0:0]
10    sync high \reset
11        update \q 1'0
12 end

```

This pass has transformed the outer RTLIL::SwitchRule into a modified RTLIL::SyncRule object for the `\reset` signal. Further processing converts the RTLIL::Process into e.g. a d-type flip-flop with asynchronous reset and a multiplexer for the enable signal:

```

1 cell $adff $procdff$6
2     parameter \ARST_POLARITY 1'1
3     parameter \ARST_VALUE 1'0
4     parameter \CLK_POLARITY 1'1
5     parameter \WIDTH 1
6     connect \ARST \reset
7     connect \CLK \clock
8     connect \D $0\q[0:0]
9     connect \Q \q
10 end
11 cell $mux $procmux$3
12     parameter \WIDTH 1

```

<sup>1</sup>The syntax `1'1` in the RTLIL code specifies a constant with a length of one bit (the first “1”), and this bit is a one (the second “1”).

```

13      connect \A \q
14      connect \B \d
15      connect \S \enable
16      connect \Y $0\q[0:0]
17 end

```

Different combinations of passes may yield different results. Note that `$adff` and `$mux` are internal cell types that still need to be mapped to cell types from the target cell library.

Some passes refuse to operate on modules that still contain RTLIL::Process objects as the presence of these objects in a module increases the complexity. Therefore the passes to translate processes to a netlist of cells are usually called early in a synthesis script. The `proc` pass calls a series of other passes that together perform this conversion in a way that is suitable for most synthesis tasks.

## 4.2.6 RTLIL::Memory

For every array (memory) in the HDL code an RTLIL::Memory object is created. A memory object has the following properties:

- The memory name
- A list of attributes
- The width of an addressable word
- The size of the memory in number of words

All read accesses to the memory are transformed to `$memrd` cells and all write accesses to `$memwr` cells by the language frontend. These cells consist of independent read- and write-ports to the memory. Memory initialization is transformed to `$meminit` cells by the language frontend. The `\MEMID` parameter on these cells is used to link them together and to the RTLIL::Memory object they belong to.

The rationale behind using separate cells for the individual ports versus creating a large multiport memory cell right in the language frontend is that the separate `$memrd` and `$memwr` cells can be consolidated using resource sharing. As resource sharing is a non-trivial optimization problem where different synthesis tasks can have different requirements it lends itself to do the optimisation in separate passes and merge the RTLIL::Memory objects and `$memrd` and `$memwr` cells to multiport memory blocks after resource sharing is completed.

The memory pass performs this conversion and can (depending on the options passed to it) transform the memories directly to d-type flip-flops and address logic or yield multiport memory blocks (represented using `$mem` cells).

See Sec. 5.1.5 for details about the memory cell types.

## 4.3 Command Interface and Synthesis Scripts

Yosys reads and processes commands from synthesis scripts, command line arguments and an interactive command prompt. Yosys commands consist of a command name and an optional whitespace separated list of arguments. Commands are terminated using the newline character or a semicolon (;). Empty lines and lines starting with the hash sign (#) are ignored. See Sec. 3.3 for an example synthesis script.

The command `help` can be used to access the command reference manual.

Most commands can operate not only on the entire design but also specifically on *selected* parts of the design. For example the command `dump` will print all selected objects in the current design while `dump foobar` will only print the module `foobar` and `dump *` will print the entire design regardless of the current selection.

The selection mechanism is very powerful. For example the command `dump */t:$add %x:[A] */w:*%i` will print all wires that are connected to the \A port of a \$add cell. Detailed documentation of the select framework can be found in the command reference for the `select` command.

## 4.4 Source Tree and Build System

The Yosys source tree is organized into the following top-level directories:

- `backends/`  
This directory contains a subdirectory for each of the backend modules.
- `frontends/`  
This directory contains a subdirectory for each of the frontend modules.
- `kernel/`  
This directory contains all the core functionality of Yosys. This includes the functions and definitions for working with the RTLIL data structures (`rtlil.h` and `rtlil.cc`), the `main()` function (`driver.cc`), the internal framework for generating log messages (`log.h` and `log.cc`), the internal framework for registering and calling passes (`register.h` and `register.cc`), some core commands that are not really passes (`select.cc`, `show.cc`, ...) and a couple of other small utility libraries.
- `passes/`  
This directory contains a subdirectory for each pass or group of passes. For example as of this writing the directory `passes/opt/` contains the code for seven passes: `opt`, `opt_expr`, `opt_muxtree`, `opt_reduce`, `opt_rmdff`, `opt_rmunused` and `opt_merge`.
- `techlibs/`  
This directory contains simulation models and standard implementations for the cells from the internal cell library.
- `tests/`  
This directory contains a couple of test cases. Most of the smaller tests are executed automatically when `make test` is called. The larger tests must be executed manually. Most of the larger tests require downloading external HDL source code and/or external tools. The tests range from comparing simulation results of the synthesized design to the original sources to logic equivalence checking of entire CPU cores.

The top-level Makefile includes `frontends/*/Makefile.inc`, `passes/*/Makefile.inc` and `backends/*/Makefile.inc`. So when extending Yosys it is enough to create a new directory in `frontends/`, `passes/` or `backends/` with your sources and a `Makefile.inc`. The Yosys kernel automatically detects all commands linked with Yosys. So it is not needed to add additional commands to a central list of commands.

Good starting points for reading example source code to learn how to write passes are `passes/opt/opt_rmdff.cc` and `passes/opt/opt_merge.cc`.

See the top-level README file for a quick *Getting Started* guide and build instructions. The Yosys build is based solely on Makefiles.

Users of the Qt Creator IDE can generate a QT Creator project file using `make qtcreator`. Users of the Eclipse IDE can use the “Makefile Project with Existing Code” project type in the Eclipse “New Project” dialog (only available after the CDT plugin has been installed) to create an Eclipse project in order to programming extensions to Yosys or just browse the Yosys code base.

## Chapter 5

# Internal Cell Library

Most of the passes in Yosys operate on netlists, i.e. they only care about the `RTLIL::Wire` and `RTLIL::Cell` objects in an `RTLIL::Module`. This chapter discusses the cell types used by Yosys to represent a behavioural design internally.

This chapter is split in two parts. In the first part the internal RTL cells are covered. These cells are used to represent the design on a coarse grain level. Like in the original HDL code on this level the cells operate on vectors of signals and complex cells like adders exist. In the second part the internal gate cells are covered. These cells are used to represent the design on a fine-grain gate-level. All cells from this category operate on single bit signals.

### 5.1 RTL Cells

Most of the RTL cells closely resemble the operators available in HDLs such as Verilog or VHDL. Therefore Verilog operators are used in the following sections to define the behaviour of the RTL cells.

Note that all RTL cells have parameters indicating the size of inputs and outputs. When passes modify RTL cells they must always keep the values of these parameters in sync with the size of the signals connected to the inputs and outputs.

Simulation models for the RTL cells can be found in the file `techlibs/common/simlib.v` in the Yosys source tree.

#### 5.1.1 Unary Operators

All unary RTL cells have one input port `\A` and one output port `\Y`. They also have the following parameters:

- `\A_SIGNED`  
Set to a non-zero value if the input `\A` is signed and therefore should be sign-extended when needed.
- `\A_WIDTH`  
The width of the input port `\A`.
- `\Y_WIDTH`  
The width of the output port `\Y`.

Table 5.1 lists all cells for unary RTL operators.

For the unary cells that output a logical value (`$reduce_and`, `$reduce_or`, `$reduce_xor`, `$reduce_xnor`, `$reduce_bool`, `$logic_not`), when the `\Y_WIDTH` parameter is greater than 1, the output is zero-extended, and only the least significant bit varies.

Verilog	Cell Type
$Y = \sim A$	\$not
$Y = +A$	\$pos
$Y = -A$	\$neg
$Y = \&A$	\$reduce_and
$Y =  A$	\$reduce_or
$Y = ^A$	\$reduce_xor
$Y = \sim^A$	\$reduce_xnor
$Y =  A$	\$reduce_bool
$Y = !A$	\$logic_not

**Table 5.1:** Cell types for unary operators with their corresponding Verilog expressions.

Note that \$reduce\_or and \$reduce\_bool actually represent the same logic function. But the HDL frontends generate them in different situations. A \$reduce\_or cell is generated when the prefix | operator is being used. A \$reduce\_bool cell is generated when a bit vector is used as a condition in an if-statement or ?: -expression.

### 5.1.2 Binary Operators

All binary RTL cells have two input ports \A and \B and one output port \Y. They also have the following parameters:

- \A\_SIGNED  
Set to a non-zero value if the input \A is signed and therefore should be sign-extended when needed.
- \A\_WIDTH  
The width of the input port \A.
- \B\_SIGNED  
Set to a non-zero value if the input \B is signed and therefore should be sign-extended when needed.
- \B\_WIDTH  
The width of the input port \B.
- \Y\_WIDTH  
The width of the output port \Y.

Table 5.2 lists all cells for binary RTL operators.

The \$shl and \$shr cells implement logical shifts, whereas the \$ssh1 and \$sshr cells implement arithmetic shifts. The \$shl and \$ssh1 cells implement the same operation. All four of these cells interpret the second operand as unsigned, and require \B\_SIGNED to be zero.

Two additional shift operator cells are available that do not directly correspond to any operator in Verilog, \$shift and \$shiftx. The \$shift cell performs a right logical shift if the second operand is positive (or unsigned), and a left logical shift if it is negative. The \$shiftx cell performs the same operation as the \$shift cell, but the vacated bit positions are filled with undef(x) bits, and corresponds to the Verilog indexed part-select expression.

For the binary cells that output a logical value (\$logic\_and, \$logic\_or, \$eqx, \$nex, \$lt, \$le, \$eq, \$ne, \$ge, \$gt), when the \Y\_WIDTH parameter is greater than 1, the output is zero-extended, and only the least significant bit varies.

Division and modulo cells are available in two rounding modes. The original \$div and \$mod cells are based on truncating division, and correspond to the semantics of the verilog / and % operators. The \$divfloor and \$modfloor cells represent flooring division and flooring modulo, the latter of which is also known as “remainder” in several languages. See table 5.3 for a side-by-side comparison between the different semantics.



Verilog	Cell Type	Verilog	Cell Type
$Y = A \& B$	<code>\$and</code>	$Y = A < B$	<code>\$lt</code>
$Y = A   B$	<code>\$or</code>	$Y = A <= B$	<code>\$le</code>
$Y = A \wedge B$	<code>\$xor</code>	$Y = A == B$	<code>\$eq</code>
$Y = A \sim \wedge B$	<code>\$xnor</code>	$Y = A != B$	<code>\$ne</code>
$Y = A << B$	<code>\$shl</code>	$Y = A >= B$	<code>\$ge</code>
$Y = A >> B$	<code>\$shr</code>	$Y = A > B$	<code>\$gt</code>
$Y = A <<< B$	<code>\$sshl</code>	$Y = A + B$	<code>\$add</code>
$Y = A >>> B$	<code>\$sshr</code>	$Y = A - B$	<code>\$sub</code>
$Y = A \&\& B$	<code>\$logic_and</code>	$Y = A * B$	<code>\$mul</code>
$Y = A    B$	<code>\$logic_or</code>	$Y = A / B$	<code>\$div</code>
$Y = A === B$	<code>\$eqx</code>	$Y = A \% B$	<code>\$mod</code>
$Y = A !== B$	<code>\$nex</code>	[N/A]	<code>\$divfloor</code>
		[N/A]	<code>\$modfloor</code>
		$Y = A ** B$	<code>\$pow</code>

**Table 5.2:** Cell types for binary operators with their corresponding Verilog expressions.

Division	Result	Truncating		Flooring	
		<code>\$div</code>	<code>\$mod</code>	<code>\$divfloor</code>	<code>\$modfloor</code>
-10 / 3	-3.3	-3	-1	-4	2
10 / -3	-3.3	-3	1	-4	-2
-10 / -3	3.3	3	-1	3	-1
10 / 3	3.3	3	1	3	1

**Table 5.3:** Comparison between different rounding modes for division and modulo cells.

### 5.1.3 Multiplexers

Multiplexers are generated by the Verilog HDL frontend for `? : -expressions`. Multiplexers are also generated by the `proc` pass to map the decision trees from `RTLIL::Process` objects to logic.

The simplest multiplexer cell type is `$mux`. Cells of this type have a `\WIDTH` parameter and data inputs `\A` and `\B` and a data output `\Y`, all of the specified width. This cell also has a single bit control input `\S`. If `\S` is 0 the value from the `\A` input is sent to the output, if it is 1 the value from the `\B` input is sent to the output. So the `$mux` cell implements the function  $Y = S ? B : A$ .

The `$pmux` cell is used to multiplex between many inputs using a one-hot select signal. Cells of this type have a `\WIDTH` and a `\S_WIDTH` parameter and inputs `\A`, `\B`, and `\S` and an output `\Y`. The `\S` input is `\S_WIDTH` bits wide. The `\A` input and the output are both `\WIDTH` bits wide and the `\B` input is `\WIDTH*\S_WIDTH` bits wide. When all bits of `\S` are zero, the value from `\A` input is sent to the output. If the  $n$ 'th bit from `\S` is set, the value  $n$ 'th `\WIDTH` bits wide slice of the `\B` input is sent to the output. When more than one bit from `\S` is set the output is undefined. Cells of this type are used to model “parallel cases” (defined by using the `parallel_case` attribute or detected by an optimization).

The `$tribuf` cell is used to implement tristate logic. Cells of this type have a `\WIDTH` parameter and inputs `\A` and `\EN` and an output `\Y`. The `\A` input and `\Y` output are `\WIDTH` bits wide, and the `\EN` input is one bit wide. When `\EN` is 0, the output `\Y` is not driven. When `\EN` is 1, the value from `\A` input is sent to the `\Y` output. Therefore, the `$tribuf` cell implements the function  $Y = EN ? A : 'bz$ .

Behavioural code with cascaded `if-then-else-` and `case-`statements usually results in trees of multiplexer cells. Many passes (from various optimizations to FSM extraction) heavily depend on these multiplexer trees to understand dependencies between signals. Therefore optimizations should not break these multiplexer trees (e.g. by replacing a multiplexer between a calculated signal and a constant zero with an `$and` gate).

### 5.1.4 Registers

SR-type latches are represented by `$sr` cells. These cells have input ports `\SET` and `\CLR` and an output port `\Q`. They have the following parameters:

- `\WIDTH`  
The width of inputs `\SET` and `\CLR` and output `\Q`.
- `\SET_POLARITY`  
The set input bits are active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.
- `\CLR_POLARITY`  
The reset input bits are active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.

Both set and reset inputs have separate bits for every output bit. When both the set and reset inputs of an `$sr` cell are active for a given bit index, the reset input takes precedence.

D-type flip-flops are represented by `$dff` cells. These cells have a clock port `\CLK`, an input port `\D` and an output port `\Q`. The following parameters are available for `$dff` cells:

- `\WIDTH`  
The width of input `\D` and output `\Q`.
- `\CLK_POLARITY`  
Clock is active on the positive edge if this parameter has the value `1'b1` and on the negative edge if this parameter is `1'b0`.

D-type flip-flops with asynchronous reset are represented by `$adff` cells. As the `$dff` cells they have `\CLK`, `\D` and `\Q` ports. In addition they also have a single-bit `\ARST` input port for the reset pin and the following additional two parameters:

- `\ARST_POLARITY`  
The asynchronous reset is active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.
- `\ARST_VALUE`  
The state of `\Q` will be set to this value when the reset is active.

Usually these cells are generated by the `proc` pass using the information in the designs `RTLIL::Process` objects.

D-type flip-flops with synchronous reset are represented by `$sdff` cells. As the `$dff` cells they have `\CLK`, `\D` and `\Q` ports. In addition they also have a single-bit `\SRST` input port for the reset pin and the following additional two parameters:

- `\SRST_POLARITY`  
The synchronous reset is active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.
- `\SRST_VALUE`  
The state of `\Q` will be set to this value when the reset is active.

Note that the `$adff` and `$sdff` cells can only be used when the reset value is constant.

D-type flip-flops with asynchronous set and reset are represented by `$dffsr` cells. As the `$dff` cells they have `\CLK`, `\D` and `\Q` ports. In addition they also have multi-bit `\SET` and `\CLR` input ports and the corresponding polarity parameters, like `$sr` cells.

D-type flip-flops with enable are represented by `$dffe`, `$adffe`, `$dffsre`, `$sdffe`, and `$sdffce` cells, which are enhanced variants of `$dff`, `$adff`, `$dffsr`, `$sdff` (with reset over enable) and `$sdff` (with enable over reset) cells, respectively. They have the same ports and parameters as their base cell. In addition they also have a single-bit `\EN` input port for the enable pin and the following parameter:

- `\EN_POLARITY`  
The enable input is active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.

D-type latches are represented by `$dlatch` cells. These cells have an enable port `\EN`, an input port `\D`, and an output port `\Q`. The following parameters are available for `$dlatch` cells:

- `\WIDTH`  
The width of input `\D` and output `\Q`.
- `\EN_POLARITY`  
The enable input is active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.

The latch is transparent when the `\EN` input is active.

D-type latches with reset are represented by `$adlatch` cells. In addition to `$dlatch` ports and parameters, they also have a single-bit `\ARST` input port for the reset pin and the following additional parameters:

- `\ARST_POLARITY`  
The asynchronous reset is active-high if this parameter has the value `1'b1` and active-low if this parameter is `1'b0`.
- `\ARST_VALUE`  
The state of `\Q` will be set to this value when the reset is active.

D-type latches with set and reset are represented by `$dlatchsr` cells. In addition to `$dlatch` ports and parameters, they also have multi-bit `\SET` and `\CLR` input ports and the corresponding polarity parameters, like `$sr` cells.

### 5.1.5 Memories

Memories are either represented using `RTLIL::Memory` objects, `$memrd`, `$memwr`, and `$meminit` cells, or by `$mem` cells alone.

In the first alternative the `RTLIL::Memory` objects hold the general metadata for the memory (bit width, size in number of words, etc.) and for each port a `$memrd` (read port) or `$memwr` (write port) cell is created. Having individual cells for read and write ports has the advantage that they can be consolidated using resource sharing passes. In some cases this drastically reduces the number of required ports on the memory cell. In this alternative, memory initialization data is represented by `$meminit` cells, which allow delaying constant folding for initialization addresses and data until after the frontend finishes.

The `$memrd` cells have a clock input `\CLK`, an enable input `\EN`, an address input `\ADDR`, and a data output `\DATA`. They also have the following parameters:

- `\MEMID`  
The name of the RTLIL::Memory object that is associated with this read port.
- `\ABITS`  
The number of address bits (width of the `\ADDR` input port).
- `\WIDTH`  
The number of data bits (width of the `\DATA` output port).
- `\CLK_ENABLE`  
When this parameter is non-zero, the clock is used. Otherwise this read port is asynchronous and the `\CLK` input is not used.
- `\CLK_POLARITY`  
Clock is active on the positive edge if this parameter has the value `1'b1` and on the negative edge if this parameter is `1'b0`.
- `\TRANSPARENT`  
If this parameter is set to `1'b1`, a read and write to the same address in the same cycle will return the new value. Otherwise the old value is returned.

The `$memwr` cells have a clock input `\CLK`, an enable input `\EN` (one enable bit for each data bit), an address input `\ADDR` and a data input `\DATA`. They also have the following parameters:

- `\MEMID`  
The name of the RTLIL::Memory object that is associated with this write port.
- `\ABITS`  
The number of address bits (width of the `\ADDR` input port).
- `\WIDTH`  
The number of data bits (width of the `\DATA` output port).
- `\CLK_ENABLE`  
When this parameter is non-zero, the clock is used. Otherwise this write port is asynchronous and the `\CLK` input is not used.
- `\CLK_POLARITY`  
Clock is active on positive edge if this parameter has the value `1'b1` and on the negative edge if this parameter is `1'b0`.
- `\PRIORITY`  
The cell with the higher integer value in this parameter wins a write conflict.

The `$meminit` cells have an address input `\ADDR` and a data input `\DATA`, with the width of the `\DATA` port equal to `\WIDTH` parameter times `\WORDS` parameter. Both of the inputs must resolve to a constant for synthesis to succeed.

- `\MEMID`  
The name of the RTLIL::Memory object that is associated with this initialization cell.
- `\ABITS`  
The number of address bits (width of the `\ADDR` input port).
- `\WIDTH`  
The number of data bits per memory location.

- `\WORDS`  
The number of consecutive memory locations initialized by this cell.
- `\PRIORITY`  
The cell with the higher integer value in this parameter wins an initialization conflict.

The HDL frontend models a memory using `RTLIL::Memory` objects and asynchronous `$memrd` and `$memwr` cells. The memory pass (i.e. its various sub-passes) migrates `$dff` cells into the `$memrd` and `$memwr` cells making them synchronous, then converts them to a single `$mem` cell and (optionally) maps this cell type to `$dff` cells for the individual words and multiplexer-based address decoders for the read and write interfaces. When the last step is disabled or not possible, a `$mem` cell is left in the design.

The `$mem` cell provides the following parameters:

- `\MEMID`  
The name of the original `RTLIL::Memory` object that became this `$mem` cell.
- `\SIZE`  
The number of words in the memory.
- `\ABITS`  
The number of address bits.
- `\WIDTH`  
The number of data bits per word.
- `\INIT`  
The initial memory contents.
- `\RD_PORTS`  
The number of read ports on this memory cell.
- `\RD_CLK_ENABLE`  
This parameter is `\RD_PORTS` bits wide, containing a clock enable bit for each read port.
- `\RD_CLK_POLARITY`  
This parameter is `\RD_PORTS` bits wide, containing a clock polarity bit for each read port.
- `\RD_TRANSPARENT`  
This parameter is `\RD_PORTS` bits wide, containing a transparent bit for each read port.
- `\WR_PORTS`  
The number of write ports on this memory cell.
- `\WR_CLK_ENABLE`  
This parameter is `\WR_PORTS` bits wide, containing a clock enable bit for each write port.
- `\WR_CLK_POLARITY`  
This parameter is `\WR_PORTS` bits wide, containing a clock polarity bit for each write port.

The `$mem` cell has the following ports:

- `\RD_CLK`  
This input is `\RD_PORTS` bits wide, containing all clock signals for the read ports.
- `\RD_EN`  
This input is `\RD_PORTS` bits wide, containing all enable signals for the read ports.

- `\RD_ADDR`  
This input is `\RD_PORTS*\ABITS` bits wide, containing all address signals for the read ports.
- `\RD_DATA`  
This input is `\RD_PORTS*\WIDTH` bits wide, containing all data signals for the read ports.
- `\WR_CLK`  
This input is `\WR_PORTS` bits wide, containing all clock signals for the write ports.
- `\WR_EN`  
This input is `\WR_PORTS*\WIDTH` bits wide, containing all enable signals for the write ports.
- `\WR_ADDR`  
This input is `\WR_PORTS*\ABITS` bits wide, containing all address signals for the write ports.
- `\WR_DATA`  
This input is `\WR_PORTS*\WIDTH` bits wide, containing all data signals for the write ports.

The `memory_collect` pass can be used to convert discrete `$memrd`, `$memwr`, and `$meminit` cells belonging to the same memory to a single `$mem` cell, whereas the `memory_unpack` pass performs the inverse operation. The `memory_dff` pass can combine asynchronous memory ports that are fed by or feeding registers into synchronous memory ports. The `memory_bram` pass can be used to recognize `$mem` cells that can be implemented with a block RAM resource on an FPGA. The `memory_map` pass can be used to implement `$mem` cells as basic logic: word-wide DFFs and address decoders.

### 5.1.6 Finite State Machines

#### FIXME:

Add a brief description of the `$fsm` cell type.

### 5.1.7 Specify rules

#### FIXME:

Add information about `$specify2`, `$specify3`, and `$specrule` cells.

### 5.1.8 Formal verification cells

#### FIXME:

Add information about `$assert`, `$assume`, `$live`, `$fair`, `$cover`, `$equiv`, `$initstate`, `$anyconst`, `$anyseq`, `$allconst`, `$allseq` cells.

#### FIXME:

Add information about `$ff` and `$_FF_` cells.

## 5.2 Gates

For gate level logic networks, fixed function single bit cells are used that do not provide any parameters.

Simulation models for these cells can be found in the file `techlibs/common/simcells.v` in the Yosys source tree.

Tables [5.4](#), [5.6](#), [5.5](#), [5.7](#), [5.8](#), [5.9](#), [5.10](#), [5.11](#) and [5.12](#) list all cell types used for gate level logic. The cell types `$_BUF_`, `$_NOT_`, `$_AND_`, `$_NAND_`, `$_ANDNOT_`, `$_OR_`, `$_NOR_`, `$_ORNOT_`, `$_XOR_`, `$_XNOR_`,

Verilog	Cell Type
<code>Y = A</code>	<code>\$_BUF_</code>
<code>Y = ~A</code>	<code>\$_NOT_</code>
<code>Y = A &amp; B</code>	<code>\$_AND_</code>
<code>Y = ~(A &amp; B)</code>	<code>\$_NAND_</code>
<code>Y = A &amp; ~B</code>	<code>\$_ANDNOT_</code>
<code>Y = A   B</code>	<code>\$_OR_</code>
<code>Y = ~(A   B)</code>	<code>\$_NOR_</code>
<code>Y = A   ~B</code>	<code>\$_ORNOT_</code>
<code>Y = A ^ B</code>	<code>\$_XOR_</code>
<code>Y = ~(A ^ B)</code>	<code>\$_XNOR_</code>
<code>Y = ~((A &amp; B)   C)</code>	<code>\$_AOI3_</code>
<code>Y = ~((A   B) &amp; C)</code>	<code>\$_OAI3_</code>
<code>Y = ~((A &amp; B)   (C &amp; D))</code>	<code>\$_AOI4_</code>
<code>Y = ~((A   B) &amp; (C   D))</code>	<code>\$_OAI4_</code>
<code>Y = S ? B : A</code>	<code>\$_MUX_</code>
<code>Y = ~(S ? B : A)</code>	<code>\$_NMUX_</code>
(see below)	<code>\$_MUX4_</code>
(see below)	<code>\$_MUX8_</code>
(see below)	<code>\$_MUX16_</code>
<code>Y = EN ? A : 1'bz</code>	<code>\$_TBUF_</code>
<b><code>always @(negedge C) Q &lt;= D</code></b>	<b><code>\$_DFF_N_</code></b>
<b><code>always @(posedge C) Q &lt;= D</code></b>	<b><code>\$_DFF_P_</code></b>
<b><code>always @* if (!E) Q &lt;= D</code></b>	<b><code>\$_DLATCH_N_</code></b>
<b><code>always @* if (E) Q &lt;= D</code></b>	<b><code>\$_DLATCH_P_</code></b>

Table 5.4: Cell types for gate level logic networks (main list)

`$_AOI3_`, `$_OAI3_`, `$_AOI4_`, `$_OAI4_`, `$_MUX_`, `$_MUX4_`, `$_MUX8_`, `$_MUX16_` and `$_NMUX_` are used to model combinatorial logic. The cell type `$_TBUF_` is used to model tristate logic.

The `$_MUX4_`, `$_MUX8_` and `$_MUX16_` cells are used to model wide muxes, and correspond to the following Verilog code:

```
// $_MUX4_
assign Y = T ? (S ? D : C) :
           (S ? B : A);

// $_MUX8_
assign Y = U ? T ? (S ? H : G) :
           (S ? F : E) :
           T ? (S ? D : C) :
           (S ? B : A);

// $_MUX16_
assign Y = V ? U ? T ? (S ? P : O) :
           (S ? N : M) :
           T ? (S ? L : K) :
           (S ? J : I) :
           U ? T ? (S ? H : G) :
           (S ? F : E) :
           T ? (S ? D : C) :
           (S ? B : A);
```

The cell types `$_DFF_N_` and `$_DFF_P_` represent d-type flip-flops.

The cell types `$_DFFE_[NP][NP]_` implement d-type flip-flops with enable. The values in the table for these cell types relate to the following Verilog code template.

<i>ClkEdge</i>	<i>RstLvl</i>	<i>RstVal</i>	Cell Type
<b>negedge</b>	0	0	<code>\$_DFF_NN0_</code> , <code>\$_SDFF_NN0_</code>
<b>negedge</b>	0	1	<code>\$_DFF_NN1_</code> , <code>\$_SDFF_NN1_</code>
<b>negedge</b>	1	0	<code>\$_DFF_NP0_</code> , <code>\$_SDFF_NP0_</code>
<b>negedge</b>	1	1	<code>\$_DFF_NP1_</code> , <code>\$_SDFF_NP1_</code>
<b>posedge</b>	0	0	<code>\$_DFF_PN0_</code> , <code>\$_SDFF_PN0_</code>
<b>posedge</b>	0	1	<code>\$_DFF_PN1_</code> , <code>\$_SDFF_PN1_</code>
<b>posedge</b>	1	0	<code>\$_DFF_PP0_</code> , <code>\$_SDFF_PP0_</code>
<b>posedge</b>	1	1	<code>\$_DFF_PP1_</code> , <code>\$_SDFF_PP1_</code>

Table 5.5: Cell types for gate level logic networks (FFs with reset)

<i>ClkEdge</i>	<i>EnLvl</i>	Cell Type
<b>negedge</b>	0	<code>\$_DFFE_NN_</code>
<b>negedge</b>	1	<code>\$_DFFE_NP_</code>
<b>posedge</b>	0	<code>\$_DFFE_PN_</code>
<b>posedge</b>	1	<code>\$_DFFE_PP_</code>

Table 5.6: Cell types for gate level logic networks (FFs with enable)

```

always @(ClkEdge C)
    if (EN == EnLvl)
        Q <= D;

```

The cell types `$_DFF_[NP][NP][01]_` implement d-type flip-flops with asynchronous reset. The values in the table for these cell types relate to the following Verilog code template, where *RstEdge* is **posedge** if *RstLvl* if 1, and **negedge** otherwise.

```

always @(ClkEdge C, RstEdge R)
    if (R == RstLvl)
        Q <= RstVal;
    else
        Q <= D;

```

The cell types `$_SDFF_[NP][NP][01]_` implement d-type flip-flops with synchronous reset. The values in the table for these cell types relate to the following Verilog code template:

```

always @(ClkEdge C)
    if (R == RstLvl)
        Q <= RstVal;
    else
        Q <= D;

```

The cell types `$_DFFE_[NP][NP][01][NP]_` implement d-type flip-flops with asynchronous reset and enable. The values in the table for these cell types relate to the following Verilog code template, where *RstEdge* is **posedge** if *RstLvl* if 1, and **negedge** otherwise.

```

always @(ClkEdge C, RstEdge R)
    if (R == RstLvl)
        Q <= RstVal;
    else if (EN == EnLvl)
        Q <= D;

```

The cell types `$_SDFFE_[NP][NP][01][NP]_` implement d-type flip-flops with synchronous reset and enable, with reset having priority over enable. The values in the table for these cell types relate to the following Verilog code template:



<i>ClkEdge</i>	<i>RstLvl</i>	<i>RstVal</i>	<i>EnLvl</i>	Cell Type
<b>negedge</b>	0	0	0	<code>\$_DFFE_NN0N_</code> , <code>\$_SDFFE_NN0N_</code> , <code>\$_SDFFCE_NN0N_</code>
<b>negedge</b>	0	0	1	<code>\$_DFFE_NN0P_</code> , <code>\$_SDFFE_NN0P_</code> , <code>\$_SDFFCE_NN0P_</code>
<b>negedge</b>	0	1	0	<code>\$_DFFE_NN1N_</code> , <code>\$_SDFFE_NN1N_</code> , <code>\$_SDFFCE_NN1N_</code>
<b>negedge</b>	0	1	1	<code>\$_DFFE_NN1P_</code> , <code>\$_SDFFE_NN1P_</code> , <code>\$_SDFFCE_NN1P_</code>
<b>negedge</b>	1	0	0	<code>\$_DFFE_NP0N_</code> , <code>\$_SDFFE_NP0N_</code> , <code>\$_SDFFCE_NP0N_</code>
<b>negedge</b>	1	0	1	<code>\$_DFFE_NP0P_</code> , <code>\$_SDFFE_NP0P_</code> , <code>\$_SDFFCE_NP0P_</code>
<b>negedge</b>	1	1	0	<code>\$_DFFE_NP1N_</code> , <code>\$_SDFFE_NP1N_</code> , <code>\$_SDFFCE_NP1N_</code>
<b>negedge</b>	1	1	1	<code>\$_DFFE_NP1P_</code> , <code>\$_SDFFE_NP1P_</code> , <code>\$_SDFFCE_NP1P_</code>
<b>posedge</b>	0	0	0	<code>\$_DFFE_PN0N_</code> , <code>\$_SDFFE_PN0N_</code> , <code>\$_SDFFCE_PN0N_</code>
<b>posedge</b>	0	0	1	<code>\$_DFFE_PN0P_</code> , <code>\$_SDFFE_PN0P_</code> , <code>\$_SDFFCE_PN0P_</code>
<b>posedge</b>	0	1	0	<code>\$_DFFE_PN1N_</code> , <code>\$_SDFFE_PN1N_</code> , <code>\$_SDFFCE_PN1N_</code>
<b>posedge</b>	0	1	1	<code>\$_DFFE_PN1P_</code> , <code>\$_SDFFE_PN1P_</code> , <code>\$_SDFFCE_PN1P_</code>
<b>posedge</b>	1	0	0	<code>\$_DFFE_PP0N_</code> , <code>\$_SDFFE_PP0N_</code> , <code>\$_SDFFCE_PP0N_</code>
<b>posedge</b>	1	0	1	<code>\$_DFFE_PP0P_</code> , <code>\$_SDFFE_PP0P_</code> , <code>\$_SDFFCE_PP0P_</code>
<b>posedge</b>	1	1	0	<code>\$_DFFE_PP1N_</code> , <code>\$_SDFFE_PP1N_</code> , <code>\$_SDFFCE_PP1N_</code>
<b>posedge</b>	1	1	1	<code>\$_DFFE_PP1P_</code> , <code>\$_SDFFE_PP1P_</code> , <code>\$_SDFFCE_PP1P_</code>

Table 5.7: Cell types for gate level logic networks (FFs with reset and enable)

<i>ClkEdge</i>	<i>SetLvl</i>	<i>RstLvl</i>	Cell Type
<b>negedge</b>	0	0	<code>\$_DFFSR_NNN_</code>
<b>negedge</b>	0	1	<code>\$_DFFSR_NNP_</code>
<b>negedge</b>	1	0	<code>\$_DFFSR_NPN_</code>
<b>negedge</b>	1	1	<code>\$_DFFSR_NPP_</code>
<b>posedge</b>	0	0	<code>\$_DFFSR_PNN_</code>
<b>posedge</b>	0	1	<code>\$_DFFSR_PNP_</code>
<b>posedge</b>	1	0	<code>\$_DFFSR_PPN_</code>
<b>posedge</b>	1	1	<code>\$_DFFSR_PPP_</code>

Table 5.8: Cell types for gate level logic networks (FFs with set and reset)

```

always @(ClkEdge C)
    if (R == RstLvl)
        Q <= RstVal;
    else if (EN == EnLvl)
        Q <= D;

```

The cell types `$_SDFFCE_[NP][NP][01][NP]_` implement d-type flip-flops with synchronous reset and enable, with enable having priority over reset. The values in the table for these cell types relate to the following Verilog code template:

```

always @(ClkEdge C)
    if (EN == EnLvl)
        if (R == RstLvl)
            Q <= RstVal;
        else
            Q <= D;

```

The cell types `$_DFFSR_[NP][NP][NP]_` implement d-type flip-flops with asynchronous set and reset. The values in the table for these cell types relate to the following Verilog code template, where *RstEdge* is **posedge** if *RstLvl* if 1, **negedge** otherwise, and *SetEdge* is **posedge** if *SetLvl* if 1, **negedge** otherwise.

```

always @(ClkEdge C, RstEdge R, SetEdge S)
    if (R == RstLvl)

```

<i>ClkEdge</i>	<i>SetLvl</i>	<i>RstLvl</i>	<i>EnLvl</i>	Cell Type
<b>negedge</b>	0	0	0	<code>\$_DFFSRE_NNNN_</code>
<b>negedge</b>	0	0	1	<code>\$_DFFSRE_NNNP_</code>
<b>negedge</b>	0	1	0	<code>\$_DFFSRE_NNPN_</code>
<b>negedge</b>	0	1	1	<code>\$_DFFSRE_NNPP_</code>
<b>negedge</b>	1	0	0	<code>\$_DFFSRE_NPNN_</code>
<b>negedge</b>	1	0	1	<code>\$_DFFSRE_NPNP_</code>
<b>negedge</b>	1	1	0	<code>\$_DFFSRE_NPPN_</code>
<b>negedge</b>	1	1	1	<code>\$_DFFSRE_NPPP_</code>
<b>posedge</b>	0	0	0	<code>\$_DFFSRE_PNNN_</code>
<b>posedge</b>	0	0	1	<code>\$_DFFSRE_PNNP_</code>
<b>posedge</b>	0	1	0	<code>\$_DFFSRE_PNPN_</code>
<b>posedge</b>	0	1	1	<code>\$_DFFSRE_PNPP_</code>
<b>posedge</b>	1	0	0	<code>\$_DFFSRE_PPNN_</code>
<b>posedge</b>	1	0	1	<code>\$_DFFSRE_PPNP_</code>
<b>posedge</b>	1	1	0	<code>\$_DFFSRE_PPPN_</code>
<b>posedge</b>	1	1	1	<code>\$_DFFSRE_PPPP_</code>

Table 5.9: Cell types for gate level logic networks (FFs with set and reset and enable)

<i>EnLvl</i>	<i>RstLvl</i>	<i>RstVal</i>	Cell Type
0	0	0	<code>\$_DLATCH_NN0_</code>
0	0	1	<code>\$_DLATCH_NN1_</code>
0	1	0	<code>\$_DLATCH_NP0_</code>
0	1	1	<code>\$_DLATCH_NP1_</code>
1	0	0	<code>\$_DLATCH_PN0_</code>
1	0	1	<code>\$_DLATCH_PN1_</code>
1	1	0	<code>\$_DLATCH_PP0_</code>
1	1	1	<code>\$_DLATCH_PP1_</code>

Table 5.10: Cell types for gate level logic networks (latches with reset)

```

        Q <= 0;
    else if (S == SetLvl)
        Q <= 1;
    else
        Q <= D;

```

The cell types `$_DFFSRE_[NP][NP][NP][NP]_` implement d-type flip-flops with asynchronous set and reset and enable. The values in the table for these cell types relate to the following Verilog code template, where *RstEdge* is **posedge** if *RstLvl* if 1, **negedge** otherwise, and *SetEdge* is **posedge** if *SetLvl* if 1, **negedge** otherwise.

```

always @(ClkEdge C, RstEdge R, SetEdge S)
    if (R == RstLvl)
        Q <= 0;
    else if (S == SetLvl)
        Q <= 1;
    else if (E == EnLvl)
        Q <= D;

```

The cell types `$_DLATCH_N_` and `$_DLATCH_P_` represent d-type latches.

The cell types `$_DLATCH_[NP][NP][01]_` implement d-type latches with reset. The values in the table for these cell types relate to the following Verilog code template:

<i>EnLvl</i>	<i>SetLvl</i>	<i>RstLvl</i>	Cell Type
0	0	0	<code>\$_DLATCHSR_NNN_</code>
0	0	1	<code>\$_DLATCHSR_NNP_</code>
0	1	0	<code>\$_DLATCHSR_NPN_</code>
0	1	1	<code>\$_DLATCHSR_NPP_</code>
1	0	0	<code>\$_DLATCHSR_PNN_</code>
1	0	1	<code>\$_DLATCHSR_PNP_</code>
1	1	0	<code>\$_DLATCHSR_PPN_</code>
1	1	1	<code>\$_DLATCHSR_PPP_</code>

**Table 5.11:** Cell types for gate level logic networks (latches with set and reset)

<i>SetLvl</i>	<i>RstLvl</i>	Cell Type
0	0	<code>\$_SR_NN_</code>
0	1	<code>\$_SR_NP_</code>
1	0	<code>\$_SR_PN_</code>
1	1	<code>\$_SR_PP_</code>

**Table 5.12:** Cell types for gate level logic networks (SR latches)

```

always @*
    if (R == RstLvl)
        Q <= RstVal;
    else if (E == EnLvl)
        Q <= D;

```

The cell types `$_DLATCHSR_[NP][NP][NP]_` implement d-type latches with set and reset. The values in the table for these cell types relate to the following Verilog code template:

```

always @*
    if (R == RstLvl)
        Q <= 0;
    else if (S == SetLvl)
        Q <= 1;
    else if (E == EnLvl)
        Q <= D;

```

The cell types `$_SR_[NP][NP]_` implement sr-type latches. The values in the table for these cell types relate to the following Verilog code template:

```

always @*
    if (R == RstLvl)
        Q <= 0;
    else if (S == SetLvl)
        Q <= 1;

```

In most cases gate level logic networks are created from RTL networks using the `techmap` pass. The flip-flop cells from the gate level logic network can be mapped to physical flip-flop cells from a Liberty file using the `dfflibmap` pass. The combinatorial logic cells can be mapped to physical cells from a Liberty file via ABC [27] using the `abc` pass.

**FIXME:**

Add information about `$slice` and `$concat` cells.

**FIXME:**

Add information about `$lut` and `$sop` cells.

**FIXME:**

Add information about `$alu`, `$macc`, `$fa`, and `$lcu` cells.

## Chapter 6

# Programming Yosys Extensions

This chapter contains some bits and pieces of information about programming yosys extensions. Also consult the section on programming in the “Yosys Presentation” (can be downloaded from the Yosys website as PDF) and don’t be afraid to ask questions on the Yosys Subreddit.

### 6.1 The “CodingReadme” File

The following is an excerpt of the CodingReadme file from the Yosys source tree.

CodingReadme

```
8 Getting Started
9 =====
10
11
12 Outline of a Yosys command
13 -----
14
15 Here is a the C++ code for a "hello_world" Yosys command (hello.cc):
16
17     #include "kernel/yosys.h"
18
19     USING_YOSYS_NAMESPACE
20     PRIVATE_NAMESPACE_BEGIN
21
22     struct HelloWorldPass : public Pass {
23         HelloWorldPass() : Pass("hello_world") { }
24         void execute(vector<string>, Design*) override {
25             log("Hello World!\n");
26         }
27     } HelloWorldPass;
28
29     PRIVATE_NAMESPACE_END
30
31 This can be built into a Yosys module using the following command:
32
33     yosys-config --exec --cxx --cxxflags --ldflags -o hello.so -shared hello.cc --
34
```

35 Or short:

```
36
37     yosys-config --build hello.so hello.cc
38
```

39 And then executed using the following command:

```
40
41     yosys -m hello.so -p hello_world
42
43
```

## 44 Yosys Data Structures

45 -----

46  
47 Here is a short list of data structures that you should make yourself familiar  
48 with before you write C++ code for Yosys. The following data structures are all  
49 defined when "kernel/yosys.h" is included and USING\_YOSYS\_NAMESPACE is used.

50

### 51 1. Yosys Container Classes

52

53 Yosys uses `dict<K, T>` and `pool<T>` as main container classes. `dict<K, T>` is  
54 essentially a replacement for `std::unordered_map<K, T>` and `pool<T>` is a  
55 replacement for `std::unordered_set<T>`. The main characteristics are:

56

- 57 - `dict<K, T>` and `pool<T>` are about 2x faster than the std containers
- 58
- 59 - references to elements in a `dict<K, T>` or `pool<T>` are invalidated by  
60 insert and remove operations (similar to `std::vector<T>` on `push_back()`).
- 61
- 62 - some iterators are invalidated by `erase()`. specifically, iterators  
63 that have not passed the erased element yet are invalidated. (`erase()`  
64 itself returns valid iterator to the next element.)
- 65
- 66 - no iterators are invalidated by `insert()`. elements are inserted at  
67 `begin()`. i.e. only a new iterator that starts at `begin()` will see the  
68 inserted elements.
- 69
- 70 - the method `.count(key, iterator)` is like `.count(key)` but only  
71 considers elements that can be reached via the iterator.
- 72
- 73 - iterators can be compared. `it1 < it2` means that the position of `t2`  
74 can be reached via `t1` but not vice versa.
- 75
- 76 - the method `.sort()` can be used to sort the elements in the container  
77 the container stays sorted until elements are added or removed.
- 78
- 79 - `dict<K, T>` and `pool<T>` will have the same order of iteration across  
80 all compilers, standard libraries and architectures.

81

82 In addition to `dict<K, T>` and `pool<T>` there is also an `idict<K>` that  
83 creates a bijective map from `K` to the integers. For example:

84

```
85     idict<string, 42> si;
86     log("%d\n", si("hello"));      // will print 42
87     log("%d\n", si("world"));      // will print 43
88     log("%d\n", si.at("world"));   // will print 43
```

```

89         log("%d\n", si.at("dummy"));    // will throw exception
90         log("%s\n", si[42].c_str());    // will print hello
91         log("%s\n", si[43].c_str());    // will print world
92         log("%s\n", si[44].c_str());    // will throw exception
93

```

94 It is not possible to remove elements from an idict.

95  
96 Finally mfp<K> implements a merge-find set data structure (aka. disjoint-set or  
97 union-find) over the type K ("mfp" = merge-find-promote).

## 98 2. Standard STL data types

99  
100 In Yosys we use std::vector<T> and std::string whenever applicable. When  
101 dict<K, T> and pool<T> are not suitable then std::map<K, T> and std::set<T>  
102 are used instead.

103  
104 The types std::vector<T> and std::string are also available as vector<T>  
105 and string in the Yosys namespace.

## 106 3. RTLIL objects

107  
108 The current design (essentially a collection of modules, each defined by a  
109 netlist) is stored in memory using RTLIL object (declared in kernel/rtlil.h,  
110 automatically included by kernel/yosys.h). You should glance over at least  
111 the declarations for the following types in kernel/rtlil.h:

112  
113  
114  
115 RTLIL::IdString

116 This is a handle for an identifier (e.g. cell or wire name).  
117 It feels a lot like a std::string, but is only a single int  
118 in size. (The actual string is stored in a global lookup  
119 table.)

120  
121 RTLIL::SigBit

122 A single signal bit. I.e. either a constant state (0, 1,  
123 x, z) or a single bit from a wire.

124  
125 RTLIL::SigSpec

126 Essentially a vector of SigBits.

127  
128 RTLIL::Wire

129 RTLIL::Cell

130 The building blocks of the netlist in a module.

131  
132 RTLIL::Module

133 RTLIL::Design

134 The module is a container with connected cells and wires  
135 in it. The design is a container with modules in it.

136  
137 All this types are also available without the RTLIL:: prefix in the Yosys  
138 namespace.

## 139 4. SigMap and other Helper Classes

140  
141  
142 There are a couple of additional helper classes that are in wide use

in Yosys. Most importantly there is SigMap (declared in kernel/sigtools.h).  
 When a design has many wires in it that are connected to each other, then a single signal bit can have multiple valid names. The SigMap object can be used to map SigSpecs or SigBits to unique SigSpecs and SigBits that consistently only use one wire from such a group of connected wires. For example:

```
SigBit a = module->addWire(NEW_ID);
SigBit b = module->addWire(NEW_ID);
module->connect(a, b);

log("%d\n", a == b); // will print 0

SigMap sigmap(module);
log("%d\n", sigmap(a) == sigmap(b)); // will print 1
```

Using the RTLIL Netlist Format

In the RTLIL netlist format the cell ports contain SigSpecs that point to the Wires. There are no references in the other direction. This has two direct consequences:

- (1) It is very easy to go from cells to wires but hard to go in the other way.
- (2) There is no danger in removing cells from the netlists, but removing wires can break the netlist format when there are still references to the wire somewhere in the netlist.

The solution to (1) is easy: Create custom indexes that allow you to make fast lookups for the wire-to-cell direction. You can either use existing generic index structures to do that (such as the ModIndex class) or write your own index. For many application it is simplest to construct a custom index. For example:

```
SigMap sigmap(module);
dict<SigBit, Cell*> sigbit_to_driver_index;

for (auto cell : module->cells())
    for (auto &conn : cell->connections())
        if (cell->output(conn.first))
            for (auto bit : sigmap(conn.second))
                sigbit_to_driver_index[bit] = cell;
```

Regarding (2): There is a general theme in Yosys that you don't remove wires from the design. You can rename them, unconnect them, but you do not actually remove the Wire object from the module. Instead you let the "clean" command take care of the dangling wires. On the other hand it is safe to remove cells (as long as you make sure this does not invalidate a custom index you are using in your code).

Example Code



The following yosys commands are a good starting point if you are looking for examples of how to use the Yosys API:

```
manual/CHAPTER_Prog/stubnets.cc
manual/PRESENTATION_Prog/my_cmd.cc
```

## Script Passes

-----

The ScriptPass base class can be used to implement passes that just call other passes, like a script. Examples for such passes are:

```
techlibs/common/prep.cc
techlibs/common/synth.cc
```

In some cases it is easier to implement such a pass as regular pass, for example when ScriptPass doesn't provide the type of flow control desired. (But many of the script passes in Yosys that don't use ScriptPass simply predate the ScriptPass base class.) Examples for such passes are:

```
passes/opt/opt.cc
passes/proc/proc.cc
```

Whether they use the ScriptPass base-class or not, a pass should always either call other passes without doing any non-trivial work itself, or should implement a non-trivial algorithm but not call any other passes. The reason for this is that this helps containing complexity in individual passes and simplifies debugging the entire system.

Exceptions to this rule should be rare and limited to cases where calling other passes is optional and only happens when requested by the user (such as for example 'techmap -autoproc'), or where it is about commands that are "top-level commands" in their own right, not components to be used in regular synthesis flows (such as the 'bugpoint' command).

A pass that would "naturally" call other passes and also do some work itself should be re-written in one of two ways:

- 1) It could be re-written as script pass with the parts that are not calls to other passes factored out into individual new passes. Usually in those cases the new sub passes share the same prefix as the top-level script pass.
- 2) It could be re-written so that it already expects the design in a certain state, expecting the calling script to set up this state before calling the pass in questions.

Many back-ends are examples for the 2nd approach. For example, 'write\_aiger' does not convert the design into AIG representation, but expects the design to be already in this form, and prints an 'Unsupported cell type' error message otherwise.

```

251 Notes on the existing codebase
252 -----
253
254 For historical reasons not all parts of Yosys adhere to the current coding
255 style. When adding code to existing parts of the system, adhere to this guide
256 for the new code instead of trying to mimic the style of the surrounding code.
257
258
259
260 Coding Style
261 =====
262
263
264 Formatting of code
265 -----
266
267 - Yosys code is using tabs for indentation. Tabs are 8 characters.
268
269 - A continuation of a statement in the following line is indented by
270   two additional tabs.
271
272 - Lines are as long as you want them to be. A good rule of thumb is
273   to break lines at about column 150.
274
275 - Opening braces can be put on the same or next line as the statement
276   opening the block (if, switch, for, while, do). Put the opening brace
277   on its own line for larger blocks, especially blocks that contains
278   blank lines.
279
280 - Otherwise stick to the Linux Kernel Coding Style:
281   https://www.kernel.org/doc/Documentation/CodingStyle
282
283
284 C++ Language
285 -----
286
287 Yosys is written in C++11. At the moment only constructs supported by
288 gcc 4.8 are allowed in Yosys code. This will change in future releases.
289
290 In general Yosys uses "int" instead of "size_t". To avoid compiler
291 warnings for implicit type casts, always use "GetSize(foo)" instead
292 of "foo.size()". (GetSize() is defined in kernel/yosys.h)
293
294 Use range-based for loops whenever applicable.

```

## 6.2 The “stubsnet” Example Module

The following is the complete code of the “stubsnet” example module. It is included in the Yosys source distribution as `manual/CHAPTER_Prog/stubnets.cc`.

```

                                     stubnets.cc
1  // This is free and unencumbered software released into the public domain.

```

```

2 //
3 // Anyone is free to copy, modify, publish, use, compile, sell, or
4 // distribute this software, either in source code form or as a compiled
5 // binary, for any purpose, commercial or non-commercial, and by any
6 // means.
7
8 #include "kernel/yosys.h"
9 #include "kernel/sigtools.h"
10
11 #include <string>
12 #include <map>
13 #include <set>
14
15 USING_YOSYS_NAMESPACE
16 PRIVATE_NAMESPACE_BEGIN
17
18 // this function is called for each module in the design
19 static void find_stub_nets(RTLIL::Design *design, RTLIL::Module *module, bool report_b
20 {
21     // use a SigMap to convert nets to a unique representation
22     SigMap sigmap(module);
23
24     // count how many times a single-bit signal is used
25     std::map<RTLIL::SigBit, int> bit_usage_count;
26
27     // count output lines for this module (needed only for summary output at the e
28     int line_count = 0;
29
30     log("Looking_for_stub_wires_in_module_%s:\n", RTLIL::id2cstr(module->name));
31
32     // For all ports on all cells
33     for (auto &cell_iter : module->cells_)
34     for (auto &conn : cell_iter.second->connections())
35     {
36         // Get the signals on the port
37         // (use sigmap to get a unique signal name)
38         RTLIL::SigSpec sig = sigmap(conn.second);
39
40         // add each bit to bit_usage_count, unless it is a constant
41         for (auto &bit : sig)
42             if (bit.wire != NULL)
43                 bit_usage_count[bit]++;
44     }
45
46     // for each wire in the module
47     for (auto &wire_iter : module->wires_)
48     {
49         RTLIL::Wire *wire = wire_iter.second;
50
51         // .. but only selected wires
52         if (!design->selected(module, wire))
53             continue;
54
55         // add +1 usage if this wire actually is a port

```

```

56      int usage_offset = wire->port_id > 0 ? 1 : 0;
57
58      // we will record which bits of the (possibly multi-bit) wire are stub
59      std::set<int> stub_bits;
60
61      // get a signal description for this wire and split it into separate b
62      RTLIL::SigSpec sig = sigmap(wire);
63
64      // for each bit (unless it is a constant):
65      // check if it is used at least two times and add to stub_bits otherw
66      for (int i = 0; i < GetSize(sig); i++)
67          if (sig[i].wire != NULL && (bit_usage_count[sig[i]] + usage_of
68              stub_bits.insert(i);
69
70      // continue if no stub bits found
71      if (stub_bits.size() == 0)
72          continue;
73
74      // report stub bits and/or stub wires, don't report single bits
75      // if called with report_bits set to false.
76      if (GetSize(stub_bits) == GetSize(sig)) {
77          log("_found_stub_wire:_%s\n", RTLIL::id2cstr(wire->name));
78      } else {
79          if (!report_bits)
80              continue;
81          log("_found_wire_with_stub_bits:_%s_", RTLIL::id2cstr(wire->
82              for (int bit : stub_bits)
83                  log("%s%d", bit == *stub_bits.begin() ? "" : ",_", bit
84              log("]\n");
85      }
86
87      // we have outputted a line, increment summary counter
88      line_count++;
89  }
90
91      // report summary
92      if (report_bits)
93          log("_found_%d_stub_wires_or_wires_with_stub_bits.\n", line_count);
94      else
95          log("_found_%d_stub_wires.\n", line_count);
96  }
97
98      // each pass contains a singleton object that is derived from Pass
99      struct StubnetsPass : public Pass {
100          StubnetsPass() : Pass("stubnets") { }
101          void execute(std::vector<std::string> args, RTLIL::Design *design) override
102          {
103              // variables to mirror information from passed options
104              bool report_bits = 0;
105
106              log_header(design, "Executing_STUBNETS_pass_(find_stub_nets).\n");
107
108              // parse options
109              size_t argidx;

```

```

110         for (argidx = 1; argidx < args.size(); argidx++) {
111             std::string arg = args[argidx];
112             if (arg == "-report_bits") {
113                 report_bits = true;
114                 continue;
115             }
116             break;
117         }
118
119         // handle extra options (e.g. selection)
120         extra_args(args, argidx, design);
121
122         // call find_stub_nets() for each module that is either
123         // selected as a whole or contains selected objects.
124         for (auto &it : design->modules_)
125             if (design->selected_module(it.first))
126                 find_stub_nets(design, it.second, report_bits);
127     }
128 } StubnetsPass;
129
130 PRIVATE_NAMESPACE_END

```

## Makefile

```

1 test: stubnets.so
2     yosys -ql test1.log -m ./stubnets.so test.v -p "stubnets"
3     yosys -ql test2.log -m ./stubnets.so test.v -p "opt;_stubnets"
4     yosys -ql test3.log -m ./stubnets.so test.v -p "techmap;_opt;_stubnets;_report_bits"
5     tail test1.log test2.log test3.log
6
7 stubnets.so: stubnets.cc
8     yosys-config --exec --cxx --cxxflags -I../.. --ldflags -o $@ -shared $^ --ldflags
9
10 clean:
11     rm -f test1.log test2.log test3.log
12     rm -f stubnets.so stubnets.d

```

## test.v

```

1 module uut(in1, in2, in3, out1, out2);
2
3 input [8:0] in1, in2, in3;
4 output [8:0] out1, out2;
5
6 assign out1 = in1 + in2 + (in3 >> 4);
7
8 endmodule

```

## Chapter 7

# The Verilog and AST Frontends

This chapter provides an overview of the implementation of the Yosys Verilog and AST frontends. The Verilog frontend reads Verilog-2005 code and creates an abstract syntax tree (AST) representation of the input. This AST representation is then passed to the AST frontend that converts it to RTLIL data, as illustrated in Fig. 7.1.

### 7.1 Transforming Verilog to AST

The *Verilog frontend* converts the Verilog sources to an internal AST representation that closely resembles the structure of the original Verilog code. The Verilog frontend consists of three components, the *Preprocessor*, the *Lexer* and the *Parser*.

The source code to the Verilog frontend can be found in `frontends/verilog/` in the Yosys source tree.

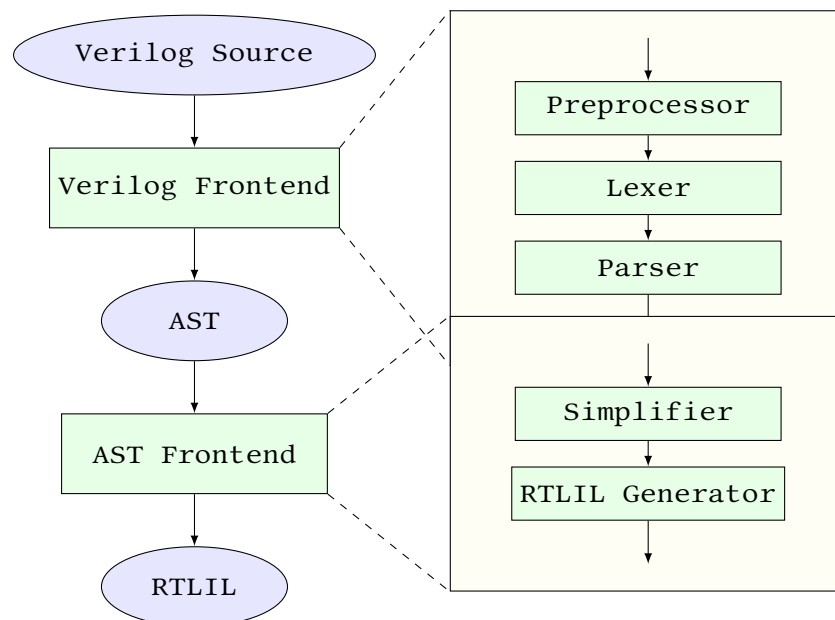


Figure 7.1: Simplified Verilog to RTLIL data flow

### 7.1.1 The Verilog Preprocessor

The Verilog preprocessor scans over the Verilog source code and interprets some of the Verilog compiler directives such as **'include**, **'define** and **'ifdef**.

It is implemented as a C++ function that is passed a file descriptor as input and returns the pre-processed Verilog code as a `std::string`.

The source code to the Verilog Preprocessor can be found in `frontends/verilog/preproc.cc` in the Yosys source tree.

### 7.1.2 The Verilog Lexer

The Verilog Lexer is written using the lexer generator *flex* [17]. Its source code can be found in `frontends/verilog/verilog_lexer.l` in the Yosys source tree. The lexer does little more than identifying all keywords and literals recognised by the Yosys Verilog frontend.

The lexer keeps track of the current location in the Verilog source code using some global variables. These variables are used by the constructor of AST nodes to annotate each node with the source code location it originated from.

Finally the lexer identifies and handles special comments such as `“//synopsys translate_off”` and `“//synopsys full_case”`. (It is recommended to use **'ifdef** constructs instead of the Synopsys `translate_on/off` comments and attributes such as `( * full_case *)` over `“//synopsys full_case”` whenever possible.)

### 7.1.3 The Verilog Parser

The Verilog Parser is written using the parser generator *bison* [18]. Its source code can be found in `frontends/verilog/verilog_parser.y` in the Yosys source tree.

It generates an AST using the `AST::AstNode` data structure defined in `frontends/ast/ast.h`. An `AST::AstNode` object has the following properties:

- **The node type**  
This enum (`AST::AstNodeType`) specifies the role of the node. Table 7.1 contains a list of all node types.
- **The child nodes**  
This is a list of pointers to all children in the abstract syntax tree.
- **Attributes**  
As almost every AST node might have Verilog attributes assigned to it, the `AST::AstNode` has direct support for attributes. Note that the attribute values are again AST nodes.
- **Node content**  
Each node might have additional content data. A series of member variables exist to hold such data. For example the member `std::string str` can hold a string value and is used e.g. in the `AST_IDENTIFIER` node type to store the identifier name.
- **Source code location**  
Each `AST::AstNode` is automatically annotated with the current source code location by the `AST::AstNode` constructor. It is stored in the `std::string filename` and `int linenum` member variables.

The `AST::AstNode` constructor can be called with up to two child nodes that are automatically added to the list of child nodes for the new object. This simplifies the creation of AST nodes for simple expressions a bit. For example the bison code for parsing multiplications:

```

1      basic_expr '*' attr basic_expr {
2          $$ = new AstNode(AST_MUL, $1, $4);
3          append_attr($$, $3);
4      } |

```

The generated AST data structure is then passed directly to the AST frontend that performs the actual conversion to RTLIL.

Note that the Yosys command `read_verilog` provides the options `-yydebug` and `-dump_ast` that can be used to print the parse tree or abstract syntax tree respectively.

## 7.2 Transforming AST to RTLIL

The *AST Frontend* converts a set of modules in AST representation to modules in RTLIL representation and adds them to the current design. This is done in two steps: *simplification* and *RTLIL generation*.

The source code to the AST frontend can be found in `frontends/ast/` in the Yosys source tree.

### 7.2.1 AST Simplification

A full-featured AST is too complex to be transformed into RTLIL directly. Therefore it must first be brought into a simpler form. This is done by calling the `AST::AstNode::simplify()` method of all `AST_MODULE` nodes in the AST. This initiates a recursive process that performs the following transformations on the AST data structure:

AST Node Type	Corresponding Verilog Construct
AST_NONE	This Node type should never be used.
AST_DESIGN	This node type is used for the top node of the AST tree. It has no corresponding Verilog construct.
AST_MODULE, AST_TASK, AST_FUNCTION	<b>module</b> , <b>task</b> and <b>function</b>
AST_WIRE	<b>input</b> , <b>output</b> , <b>wire</b> , <b>reg</b> and <b>integer</b>
AST_MEMORY	Verilog Arrays
AST_AUTOWIRE	Created by the simplifier when an undeclared signal name is used.
AST_PARAMETER, AST_LOCALPARAM	<b>parameter</b> and <b>localparam</b>
AST_PARASET	Parameter set in cell instantiation
AST_ARGUMENT	Port connection in cell instantiation
AST_RANGE	Bit-Index in a signal or element index in array
AST_CONSTANT	A literal value
AST_CELLTYPE	The type of cell in cell instantiation
AST_IDENTIFIER	An Identifier (signal name in expression or cell/task/etc. name in other contexts)
AST_PREFIX	Construct an identifier in the form <code>&lt;prefix&gt;[&lt;index&gt;].&lt;suffix&gt;</code> (used only in advanced generate constructs)
AST_FCALL, AST_TCALL	Call to function or task
AST_TO_SIGNED, AST_TO_UNSIGNED	The <code>\$signed()</code> and <code>\$unsigned()</code> functions

**Table 7.1:** AST node types with their corresponding Verilog constructs.  
(continued on next page)



AST Node Type	Corresponding Verilog Construct
AST_CONCAT AST_REPLICATE	The <code>{ . . . }</code> and <code>{ . . . { . . . } }</code> operators
AST_BIT_NOT, AST_BIT_AND, AST_BIT_OR, AST_BIT_XOR, AST_BIT_XNOR	The bitwise operators <code>~, &amp;,  , ^</code> and <code>~^</code>
AST_REDUCE_AND, AST_REDUCE_OR, AST_REDUCE_XOR, AST_REDUCE_XNOR	The unary reduction operators <code>~, &amp;,  , ^</code> and <code>~^</code>
AST_REDUCE_BOOL	Conversion from multi-bit value to boolean value (equivalent to <code>AST_REDUCE_OR</code> )
AST_SHIFT_LEFT, AST_SHIFT_RIGHT, AST_SHIFT_SLEFT, AST_SHIFT_SRIGHT	The shift operators <code>&lt;&lt;, &gt;&gt;, &lt;&lt;&lt; and &gt;&gt;&gt;</code>
AST_LT, AST_LE, AST_EQ, AST_NE, AST_GE, AST_GT	The relational operators <code>&lt;, &lt;=, ==, !=, &gt;= and &gt;</code>
AST_ADD, AST_SUB, AST_MUL, AST_DIV, AST_MOD, AST_POW	The binary operators <code>+, -, *, /, %</code> and <code>**</code>
AST_POS, AST_NEG	The prefix operators <code>+</code> and <code>-</code>
AST_LOGIC_AND, AST_LOGIC_OR, AST_LOGIC_NOT	The logic operators <code>&amp;&amp;,   </code> and <code>!</code>
AST_TERNARY	The ternary <code>? :-</code> operator
AST_MEMRD AST_MEMWR	Read and write memories. These nodes are generated by the AST simplifier for writes/reads to/from Verilog arrays.
AST_ASSIGN	An <b>assign</b> statement
AST_CELL	A cell instantiation
AST_PRIMITIVE	A primitive cell ( <b>and</b> , <b>nand</b> , <b>or</b> , etc.)
AST_ALWAYS, AST_INITIAL	Verilog <b>always</b> - and <b>initial</b> -blocks
AST_BLOCK	A <b>begin-end</b> -block
AST_ASSIGN_EQ, AST_ASSIGN_LE	Blocking ( <code>=</code> ) and nonblocking ( <code>&lt;=</code> ) assignments within an <b>always</b> - or <b>initial</b> -block
AST_CASE, AST_COND, AST_DEFAULT	The <b>case (if)</b> statements, conditions within a case and the default case respectively
AST_FOR	A <b>for</b> -loop with an <b>always</b> - or <b>initial</b> -block
AST_GENVAR, AST_GENBLOCK, AST_GENFOR, AST_GENIF	The <b>genvar</b> and <b>generate</b> keywords and <b>for</b> and <b>if</b> within a generate block.
AST_POSEDGE, AST_NEGEDGE, AST_EDGE	Event conditions for <b>always</b> blocks.

**Table 7.1:** AST node types with their corresponding Verilog constructs.  
(continuation from previous page)

- Inline all task and function calls.
- Evaluate all **generate**-statements and unroll all **for**-loops.
- Perform const folding where it is necessary (e.g. in the value part of `AST_PARAMETER`, `AST_LOCALPARAM`, `AST_PARASET` and `AST_RANGE` nodes).
- Replace `AST_PRIMITIVE` nodes with appropriate `AST_ASSIGN` nodes.
- Replace dynamic bit ranges in the left-hand-side of assignments with `AST_CASE` nodes with `AST_COND` children for each possible case.

- Detect array access patterns that are too complicated for the RTLIL::Memory abstraction and replace them with a set of signals and cases for all reads and/or writes.
- Otherwise replace array accesses with AST\_MEMRD and AST\_MEMWR nodes.

In addition to these transformations, the simplifier also annotates the AST with additional information that is needed for the RTLIL generator, namely:

- All ranges (width of signals and bit selections) are not only const folded but (when a constant value is found) are also written to member variables in the AST\_RANGE node.
- All identifiers are resolved and all AST\_IDENTIFIER nodes are annotated with a pointer to the AST node that contains the declaration of the identifier. If no declaration has been found, an AST\_AUTOWIRE node is created and used for the annotation.

This produces an AST that is fairly easy to convert to the RTLIL format.

### 7.2.2 Generating RTLIL

After AST simplification, the AST::AstNode::genRTLIL() method of each AST\_MODULE node in the AST is called. This initiates a recursive process that generates equivalent RTLIL data for the AST data.

The AST::AstNode::genRTLIL() method returns an RTLIL::SigSpec structure. For nodes that represent expressions (operators, constants, signals, etc.), the cells needed to implement the calculation described by the expression are created and the resulting signal is returned. That way it is easy to generate the circuits for large expressions using depth-first recursion. For nodes that do not represent an expression (such as AST\_CELL), the corresponding circuit is generated and an empty RTLIL::SigSpec is returned.

## 7.3 Synthesizing Verilog always Blocks

For behavioural Verilog code (code utilizing **always**- and **initial**-blocks) it is necessary to also generate RTLIL::Process objects. This is done in the following way:

- Whenever AST::AstNode::genRTLIL() encounters an **always**- or **initial**-block, it creates an instance of AST\_INTERNAL::ProcessGenerator. This object then generates the RTLIL::Process object for the block. It also calls AST::AstNode::genRTLIL() for all right-hand-side expressions contained within the block.
- First the AST\_INTERNAL::ProcessGenerator creates a list of all signals assigned within the block. It then creates a set of temporary signals using the naming scheme \$<number>\<original\_name> for each of the assigned signals.
- Then an RTLIL::Process is created that assigns all intermediate values for each left-hand-side signal to the temporary signal in its RTLIL::CaseRule/RTLIL::SwitchRule tree.
- Finally a RTLIL::SyncRule is created for the RTLIL::Process that assigns the temporary signals for the final values to the actual signals.
- Calls to AST::AstNode::genRTLIL() are generated for right hand sides as needed. When blocking assignments are used, AST::AstNode::genRTLIL() is configured using global variables to use the temporary signals that hold the correct intermediate values whenever one of the previously assigned signals is used in an expression.

Unfortunately the generation of a correct RTLIL::CaseRule/RTLIL::SwitchRule tree for behavioural code is a non-trivial task. The AST frontend solves the problem using the approach described on the following pages. The following example illustrates what the algorithm is supposed to do. Consider the following Verilog code:

```

1  always @(posedge clock) begin
2      out1 = in1;
3      if (in2)
4          out1 = !out1;
5      out2 <= out1;
6      if (in3)
7          out2 <= out2;
8      if (in4)
9          if (in5)
10             out3 <= in6;
11             else
12                 out3 <= in7;
13      out1 = out1 ^ out2;
14  end

```

This is translated by the Verilog and AST frontends into the following RTLIL code (attributes, cell parameters and wire declarations not included):

```

1  cell $logic_not $logic_not$<input>:4$2
2      connect \A \in1
3      connect \Y $logic_not$<input>:4$2_Y
4  end
5  cell $xor $xor$<input>:13$3
6      connect \A $1\out1[0:0]
7      connect \B \out2
8      connect \Y $xor$<input>:13$3_Y
9  end
10 process $proc$<input>:1$1
11     assign $0\out3[0:0] \out3
12     assign $0\out2[0:0] $1\out1[0:0]
13     assign $0\out1[0:0] $xor$<input>:13$3_Y
14     switch \in2
15         case 1'1
16             assign $1\out1[0:0] $logic_not$<input>:4$2_Y
17         case
18             assign $1\out1[0:0] \in1
19     end
20     switch \in3
21         case 1'1
22             assign $0\out2[0:0] \out2
23         case
24     end
25     switch \in4
26         case 1'1
27             switch \in5
28                 case 1'1
29                     assign $0\out3[0:0] \in6
30                 case
31                     assign $0\out3[0:0] \in7
32     end

```

```

33     case
34 end
35 sync posedge \clock
36     update \out1 $0\out1[0:0]
37     update \out2 $0\out2[0:0]
38     update \out3 $0\out3[0:0]
39 end

```

Note that the two operators are translated into separate cells outside the generated process. The signal `out1` is assigned using blocking assignments and therefore `out1` has been replaced with a different signal in all expressions after the initial assignment. The signal `out2` is assigned using nonblocking assignments and therefore is not substituted on the right-hand-side expressions.

The `RTLIL::CaseRule`/`RTLIL::SwitchRule` tree must be interpreted the following way:

- On each case level (the body of the process is the *root case*), first the actions on this level are evaluated and then the switches within the case are evaluated. (Note that the last assignment on line 13 of the Verilog code has been moved to the beginning of the RTLIL process to line 13 of the RTLIL listing.)

I.e. the special cases deeper in the switch hierarchy override the defaults on the upper levels. The assignments in lines 12 and 22 of the RTLIL code serve as an example for this.

Note that in contrast to this, the order within the `RTLIL::SwitchRule` objects within a `RTLIL::CaseRule` is preserved with respect to the original AST and Verilog code.

- The whole `RTLIL::CaseRule`/`RTLIL::SwitchRule` tree describes an asynchronous circuit. I.e. the decision tree formed by the switches can be seen independently for each assigned signal. Whenever one assigned signal changes, all signals that depend on the changed signals are to be updated. For example the assignments in lines 16 and 18 in the RTLIL code in fact influence the assignment in line 12, even though they are in the “wrong order”.

The only synchronous part of the process is in the `RTLIL::SyncRule` object generated at line 35 in the RTLIL code. The sync rule is the only part of the process where the original signals are assigned. The synchronization event from the original Verilog code has been translated into the synchronization type (`posedge`) and signal (`\clock`) for the `RTLIL::SyncRule` object. In the case of this simple example the `RTLIL::SyncRule` object is later simply transformed into a set of d-type flip-flops and the `RTLIL::CaseRule`/`RTLIL::SwitchRule` tree to a decision tree using multiplexers.

In more complex examples (e.g. asynchronous resets) the part of the `RTLIL::CaseRule`/`RTLIL::SwitchRule` tree that describes the asynchronous reset must first be transformed to the correct `RTLIL::SyncRule` objects. This is done by the `proc_adff` pass.

### 7.3.1 The ProcessGenerator Algorithm

The `AST_INTERNAL::ProcessGenerator` uses the following internal state variables:

- `subst_rvalue_from` and `subst_rvalue_to`  
These two variables hold the replacement pattern that should be used by `AST::AstNode::genRTLIL()` for signals with blocking assignments. After initialization of `AST_INTERNAL::ProcessGenerator` these two variables are empty.
- `subst_lvalue_from` and `subst_lvalue_to`  
These two variables contain the mapping from left-hand-side signals (`\<name>`) to the current temporary signal for the same thing (initially `$0\<name>`).

- `current_case`

A pointer to a `RTLIL::CaseRule` object. Initially this is the root case of the generated `RTLIL::Process`.

As the algorithm runs these variables are continuously modified as well as pushed to the stack and later restored to their earlier values by popping from the stack.

On startup the `ProcessGenerator` generates a new `RTLIL::Process` object with an empty root case and initializes its state variables as described above. Then the `RTLIL::SyncRule` objects are created using the synchronization events from the `AST_ALWAYS` node and the initial values of `subst_lvalue_from` and `subst_lvalue_to`. Then the AST for this process is evaluated recursively.

During this recursive evaluation, three different relevant types of AST nodes can be discovered: `AST_ASSIGN_LE` (nonblocking assignments), `AST_ASSIGN_EQ` (blocking assignments) and `AST_CASE` (**if** or **case** statement).

### 7.3.1.1 Handling of Nonblocking Assignments

When an `AST_ASSIGN_LE` node is discovered, the following actions are performed by the `ProcessGenerator`:

- The left-hand-side is evaluated using `AST::AstNode::genRTLIL()` and mapped to a temporary signal name using `subst_lvalue_from` and `subst_lvalue_to`.
- The right-hand-side is evaluated using `AST::AstNode::genRTLIL()`. For this call, the values of `subst_rvalue_from` and `subst_rvalue_to` are used to map blocking-assigned signals correctly.
- Remove all assignments to the same left-hand-side as this assignment from the `current_case` and all cases within it.
- Add the new assignment to the `current_case`.

### 7.3.1.2 Handling of Blocking Assignments

When an `AST_ASSIGN_EQ` node is discovered, the following actions are performed by the `ProcessGenerator`:

- Perform all the steps that would be performed for a nonblocking assignment (see above).
- Remove the found left-hand-side (before lvalue mapping) from `subst_rvalue_from` and also remove the respective bits from `subst_rvalue_to`.
- Append the found left-hand-side (before lvalue mapping) to `subst_rvalue_from` and append the found right-hand-side to `subst_rvalue_to`.

### 7.3.1.3 Handling of Cases and if-Statements

When an `AST_CASE` node is discovered, the following actions are performed by the `ProcessGenerator`:

- The values of `subst_rvalue_from`, `subst_rvalue_to`, `subst_lvalue_from` and `subst_lvalue_to` are pushed to the stack.
- A new `RTLIL::SwitchRule` object is generated, the selection expression is evaluated using `AST::AstNode::genRTLIL()` (with the use of `subst_rvalue_from` and `subst_rvalue_to`) and added to the `RTLIL::SwitchRule` object and the object is added to the `current_case`.

- All lvalues assigned to within the AST\_CASE node using blocking assignments are collected and saved in the local variable `this_case_eq_lvalue`.
- New temporary signals are generated for all signals in `this_case_eq_lvalue` and stored in `this_case_eq_ltemp`.
- The signals in `this_case_eq_lvalue` are mapped using `subst_rvalue_from` and `subst_rvalue_to` and the resulting set of signals is stored in `this_case_eq_rvalue`.

Then the following steps are performed for each AST\_COND node within the AST\_CASE node:

- Set `subst_rvalue_from`, `subst_rvalue_to`, `subst_lvalue_from` and `subst_lvalue_to` to the values that have been pushed to the stack.
- Remove `this_case_eq_lvalue` from `subst_lvalue_from/subst_lvalue_to`.
- Append `this_case_eq_lvalue` to `subst_lvalue_from` and append `this_case_eq_ltemp` to `subst_lvalue_to`.
- Push the value of `current_case`.
- Create a new RTLIL::CaseRule. Set `current_case` to the new object and add the new object to the RTLIL::SwitchRule created above.
- Add an assignment from `this_case_eq_rvalue` to `this_case_eq_ltemp` to the new `current_case`.
- Evaluate the compare value for this case using `AST::AstNode::genRTLIL()` (with the use of `subst_rvalue_from` and `subst_rvalue_to`) modify the new `current_case` accordingly.
- Recursion into the children of the AST\_COND node.
- Restore `current_case` by popping the old value from the stack.

Finally the following steps are performed:

- The values of `subst_rvalue_from`, `subst_rvalue_to`, `subst_lvalue_from` and `subst_lvalue_to` are popped from the stack.
- The signals from `this_case_eq_lvalue` are removed from the `subst_rvalue_from/subst_rvalue_to`-pair.
- The value of `this_case_eq_lvalue` is appended to `subst_rvalue_from` and the value of `this_case_eq_ltemp` is appended to `subst_rvalue_to`.
- Map the signals in `this_case_eq_lvalue` using `subst_lvalue_from/subst_lvalue_to`.
- Remove all assignments to signals in `this_case_eq_lvalue` in `current_case` and all cases within it.
- Add an assignment from `this_case_eq_ltemp` to `this_case_eq_lvalue` to `current_case`.

#### 7.3.1.4 Further Analysis of the Algorithm for Cases and if-Statements

With respect to nonblocking assignments the algorithm is easy: later assignments invalidate earlier assignments. For each signal assigned using nonblocking assignments exactly one temporary variable is generated (with the \$0-prefix) and this variable is used for all assignments of the variable.

Note how all the `_eq_`-variables become empty when no blocking assignments are used and many of the steps in the algorithm can then be ignored as a result of this.

For a variable with blocking assignments the algorithm shows the following behaviour: First a new temporary variable is created. This new temporary variable is then registered as the assignment target for all assignments for this variable within the cases for this `AST_CASE` node. Then for each case the new temporary variable is first assigned the old temporary variable. This assignment is overwritten if the variable is actually assigned in this case and is kept as a default value otherwise.

This yields an `RTLIL::CaseRule` that assigns the new temporary variable in all branches. So when all cases have been processed a final assignment is added to the containing block that assigns the new temporary variable to the old one. Note how this step always overrides a previous assignment to the old temporary variable. Other than nonblocking assignments, the old assignment could still have an effect somewhere in the design, as there have been calls to `AST::AstNode::genRTLIL()` with a `subst_rvalue_from/subst_rvalue_to`-tuple that contained the right-hand-side of the old assignment.

### 7.3.2 The proc pass

The `ProcessGenerator` converts a behavioural model in AST representation to a behavioural model in `RTLIL::Process` representation. The actual conversion from a behavioural model to an RTL representation is performed by the `proc` pass and the passes it launches:

- `proc_clean` and `proc_rmdead`  
These two passes just clean up the `RTLIL::Process` structure. The `proc_clean` pass removes empty parts (eg. empty assignments) from the process and `proc_rmdead` detects and removes unreachable branches from the process's decision trees.
- `proc_arst`  
This pass detects processes that describe d-type flip-flops with asynchronous resets and rewrites the process to better reflect what they are modelling: Before this pass, an asynchronous reset has two edge-sensitive sync rules and one top-level `RTLIL::SwitchRule` for the reset path. After this pass the sync rule for the reset is level-sensitive and the top-level `RTLIL::SwitchRule` has been removed.
- `proc_mux`  
This pass converts the `RTLIL::CaseRule/RTLIL::SwitchRule`-tree to a tree of multiplexers per written signal. After this, the `RTLIL::Process` structure only contains the `RTLIL::SyncRules` that describe the output registers.
- `proc_dff`  
This pass replaces the `RTLIL::SyncRules` to d-type flip-flops (with asynchronous resets if necessary).
- `proc_clean`  
A final call to `proc_clean` removes the now empty `RTLIL::Process` objects.

Performing these last processing steps in passes instead of in the Verilog frontend has two important benefits:

First it improves the transparency of the process. Everything that happens in a separate pass is easier to debug, as the RTLIL data structures can be easily investigated before and after each of the steps.

Second it improves flexibility. This scheme can easily be extended to support other types of storage-elements, such as sr-latches or d-latches, without having to extend the actual Verilog frontend.

## 7.4 Synthesizing Verilog Arrays

### FIXME:

Add some information on the generation of `$memrd` and `$memwr` cells and how they are processed in the memory pass.

## 7.5 Synthesizing Parametric Designs

### FIXME:

Add some information on the `RTLIL::Module::derive()` method and how it is used to synthesize parametric modules via the `hierarchy` pass.



## Chapter 8

# Optimizations

Yosys employs a number of optimizations to generate better and cleaner results. This chapter outlines these optimizations.

### 8.1 Simple Optimizations

The Yosys pass `opt` runs a number of simple optimizations. This includes removing unused signals and cells and const folding. It is recommended to run this pass after each major step in the synthesis script. At the time of this writing the `opt` pass executes the following passes that each perform a simple optimization:

- Once at the beginning of `opt`:
  - `opt_expr`
  - `opt_merge -nomux`
- Repeat until result is stable:
  - `opt_muxtree`
  - `opt_reduce`
  - `opt_merge`
  - `opt_rmdff`
  - `opt_clean`
  - `opt_expr`

The following section describes each of the `opt_*` passes.

#### 8.1.1 The `opt_expr` pass

This pass performs const folding on the internal combinational cell types described in Chap. 5. This means a cell with all constant inputs is replaced with the constant value this cell drives. In some cases this pass can also optimize cells with some constant inputs.

Table 8.1 shows the replacement rules used for optimizing an `$_AND_` gate. The first three rules implement the obvious const folding rules. Note that ‘any’ might include dynamic values calculated by other parts of the circuit. The following three lines propagate undef (X) states. These are the only three cases in which it is allowed to propagate an undef according to Sec. 5.1.10 of IEEE Std. 1364-2005 [Ver06].

A-Input	B-Input	Replacement
any	0	0
0	any	0
1	1	1
X/Z	X/Z	X
1	X/Z	X
X/Z	1	X
any	X/Z	0
X/Z	any	0
$a$	1	$a$
1	$b$	$b$

**Table 8.1:** Const folding rules for `$_AND_` cells as used in `opt_expr`.

The next two lines assume the value 0 for undef states. These two rules are only used if no other substitutions are possible in the current module. If other substitutions are possible they are performed first, in the hope that the ‘any’ will change to an undef value or a 1 and therefore the output can be set to undef.

The last two lines simply replace an `$_AND_` gate with one constant-1 input with a buffer.

Besides this basic const folding the `opt_expr` pass can replace 1-bit wide `$eq` and `$ne` cells with buffers or not-gates if one input is constant.

The `opt_expr` pass is very conservative regarding optimizing `$mux` cells, as these cells are often used to model decision-trees and breaking these trees can interfere with other optimizations.

### 8.1.2 The `opt_muxtree` pass

This pass optimizes trees of multiplexer cells by analyzing the select inputs. Consider the following simple example:

```

1 module uut(a, y);
2 input a;
3 output [1:0] y = a ? (a ? 1 : 2) : 3;
4 endmodule
```

The output can never be 2, as this would require  $a$  to be 1 for the outer multiplexer and 0 for the inner multiplexer. The `opt_muxtree` pass detects this contradiction and replaces the inner multiplexer with a constant 1, yielding the logic for  $y = a ? 1 : 3$ .

### 8.1.3 The `opt_reduce` pass

This is a simple optimization pass that identifies and consolidates identical input bits to `$reduce_and` and `$reduce_or` cells. It also sorts the input bits to ease identification of shareable `$reduce_and` and `$reduce_or` cells in other passes.

This pass also identifies and consolidates identical inputs to multiplexer cells. In this case the new shared select bit is driven using a `$reduce_or` cell that combines the original select bits.

Lastly this pass consolidates trees of `$reduce_and` cells and trees of `$reduce_or` cells to single large `$reduce_and` or `$reduce_or` cells.

These three simple optimizations are performed in a loop until a stable result is produced.

### 8.1.4 The `opt_rmdff` pass

This pass identifies single-bit d-type flip-flops (`$_DFF_*`, `$dff`, and `$adff` cells) with a constant data input and replaces them with a constant driver.

### 8.1.5 The `opt_clean` pass

This pass identifies unused signals and cells and removes them from the design. It also creates an `\unused_bits` attribute on wires with unused bits. This attribute can be used for debugging or by other optimization passes.

### 8.1.6 The `opt_merge` pass

This pass performs trivial resource sharing. This means that this pass identifies cells with identical inputs and replaces them with a single instance of the cell.

The option `-nomux` can be used to disable resource sharing for multiplexer cells (`$mux` and `$pmux`). This can be useful as it prevents multiplexer trees to be merged, which might prevent `opt_muxtree` to identify possible optimizations.

## 8.2 FSM Extraction and Encoding

The `fsm` pass performs finite-state-machine (FSM) extraction and recoding. The `fsm` pass simply executes the following other passes:

- Identify and extract FSMs:
  - `fsm_detect`
  - `fsm_extract`
- Basic optimizations:
  - `fsm_opt`
  - `opt_clean`
  - `fsm_opt`
- Expanding to nearby gate-logic (if called with `-expand`):
  - `fsm_expand`
  - `opt_clean`
  - `fsm_opt`
- Re-code FSM states (unless called with `-norecode`):
  - `fsm_recode`
- Print information about FSMs:
  - `fsm_info`
- Export FSMs in KISS2 file format (if called with `-export`):
  - `fsm_export`
- Map FSMs to RTL cells (unless called with `-nomap`):

### – fsm\_map

The `fsm_detect` pass identifies FSM state registers and marks them using the `\fsm_encoding= "auto"` attribute. The `fsm_extract` extracts all FSMs marked using the `\fsm_encoding` attribute (unless `\fsm_encoding` is set to "none") and replaces the corresponding RTL cells with a `$fsm` cell. All other `fsm_*` passes operate on these `$fsm` cells. The `fsm_map` call finally replaces the `$fsm` cells with RTL cells.

Note that these optimizations operate on an RTL netlist. I.e. the `fsm` pass should be executed after the `proc` pass has transformed all `RTLIL::Process` objects to RTL cells.

The algorithms used for FSM detection and extraction are influenced by a more general reported technique [STGR10].

## 8.2.1 FSM Detection

The `fsm_detect` pass identifies FSM state registers. It sets the `\fsm_encoding= "auto"` attribute on any (multi-bit) wire that matches the following description:

- Does not already have the `\fsm_encoding` attribute.
- Is not an output of the containing module.
- Is driven by single `$dff` or `$adff` cell.
- The `\D-Input` of this `$dff` or `$adff` cell is driven by a multiplexer tree that only has constants or the old state value on its leaves.
- The state value is only used in the said multiplexer tree or by simple relational cells that compare the state value to a constant (usually `$eq` cells).

This heuristic has proven to work very well. It is possible to overwrite it by setting `\fsm_encoding= "auto"` on registers that should be considered FSM state registers and setting `\fsm_encoding= "none"` on registers that match the above criteria but should not be considered FSM state registers.

Note however that marking state registers with `\fsm_encoding` that are not suitable for FSM recoding can cause synthesis to fail or produce invalid results.

## 8.2.2 FSM Extraction

The `fsm_extract` pass operates on all state signals marked with the `\fsm_encoding (!= "none")` attribute. For each state signal the following information is determined:

- The state registers
- The asynchronous reset state if the state registers use asynchronous reset
- All states and the control input signals used in the state transition functions
- The control output signals calculated from the state signals and control inputs
- A table of all state transitions and corresponding control inputs- and outputs

The state registers (and asynchronous reset state, if applicable) is simply determined by identifying the driver for the state signal.

From there the \$mux-tree driving the state register inputs is recursively traversed. All select inputs are control signals and the leaves of the \$mux-tree are the states. The algorithm fails if a non-constant leaf that is not the state signal itself is found.

The list of control outputs is initialized with the bits from the state signal. It is then extended by adding all values that are calculated by cells that compare the state signal with a constant value.

In most cases this will cover all uses of the state register, thus rendering the state encoding arbitrary. If however a design uses e.g. a single bit of the state value to drive a control output directly, this bit of the state signal will be transformed to a control output of the same value.

Finally, a transition table for the FSM is generated. This is done by using the `ConstEval` C++ helper class (defined in `kernel/consteval.h`) that can be used to evaluate parts of the design. The `ConstEval` class can be asked to calculate a given set of result signals using a set of signal-value assignments. It can also be passed a list of stop-signals that abort the `ConstEval` algorithm if the value of a stop-signal is needed in order to calculate the result signals.

The `fsm_extract` pass uses the `ConstEval` class in the following way to create a transition table. For each state:

1. Create a `ConstEval` object for the module containing the FSM
2. Add all control inputs to the list of stop signals
3. Set the state signal to the current state
4. Try to evaluate the next state and control output
5. If step 4 was not successful:
  - Recursively goto step 4 with the offending stop-signal set to 0.
  - Recursively goto step 4 with the offending stop-signal set to 1.
6. If step 4 was successful: Emit transition

Finally a `$fsm` cell is created with the generated transition table and added to the module. This new cell is connected to the control signals and the old drivers for the control outputs are disconnected.

### 8.2.3 FSM Optimization

The `fsm_opt` pass performs basic optimizations on `$fsm` cells (not including state recoding). The following optimizations are performed (in this order):

- Unused control outputs are removed from the `$fsm` cell. The attribute `\unused_bits` (that is usually set by the `opt_clean` pass) is used to determine which control outputs are unused.
- Control inputs that are connected to the same driver are merged.
- When a control input is driven by a control output, the control input is removed and the transition table altered to give the same performance without the external feedback path.
- Entries in the transition table that yield the same output and only differ in the value of a single control input bit are merged and the different bit is removed from the sensitivity list (turned into a don't-care bit).
- Constant inputs are removed and the transition table is altered to give an unchanged behaviour.
- Unused inputs are removed.

### 8.2.4 FSM Recoding

The `fsm_recode` pass assigns new bit pattern to the states. Usually this also implies a change in the width of the state signal. At the moment of this writing only one-hot encoding with all-zero for the reset state is supported.

The `fsm_recode` pass can also write a text file with the changes performed by it that can be used when verifying designs synthesized by Yosys using Synopsys Formality [24].

## 8.3 Logic Optimization

Yosys can perform multi-level combinational logic optimization on gate-level netlists using the external program ABC [27]. The `abc` pass extracts the combinational gate-level parts of the design, passes it through ABC, and re-integrates the results. The `abc` pass can also be used to perform other operations using ABC, such as technology mapping (see Sec. 9.3 for details).

## Chapter 9

# Technology Mapping

Previous chapters outlined how HDL code is transformed into an RTL netlist. The RTL netlist is still based on abstract coarse-grain cell types like arbitrary width adders and even multipliers. This chapter covers how an RTL netlist is transformed into a functionally equivalent netlist utilizing the cell types available in the target architecture.

Technology mapping is often performed in two phases. In the first phase RTL cells are mapped to an internal library of single-bit cells (see Sec. 5.2). In the second phase this netlist of internal gate types is transformed to a netlist of gates from the target technology library.

When the target architecture provides coarse-grain cells (such as block ram or ALUs), these must be mapped to directly from the RTL netlist, as information on the coarse-grain structure of the design is lost when it is mapped to bit-width gate types.

### 9.1 Cell Substitution

The simplest form of technology mapping is cell substitution, as performed by the `techmap` pass. This pass, when provided with a Verilog file that implements the RTL cell types using simpler cells, simply replaces the RTL cells with the provided implementation.

When no map file is provided, `techmap` uses a built-in map file that maps the Yosys RTL cell types to the internal gate library used by Yosys. The curious reader may find this map file as `techlibs/common/techmap.v` in the Yosys source tree.

Additional features have been added to `techmap` to allow for conditional mapping of cells (see `help techmap` or Sec. C.190). This can for example be useful if the target architecture supports hardware multipliers for certain bit-widths but not for others.

A usual synthesis flow would first use the `techmap` pass to directly map some RTL cells to coarse-grain cells provided by the target architecture (if any) and then use `techmap` with the built-in default file to map the remaining RTL cells to gate logic.

### 9.2 Subcircuit Substitution

Sometimes the target architecture provides cells that are more powerful than the RTL cells used by Yosys. For example a cell in the target architecture that can calculate the absolute-difference of two numbers does not match any single RTL cell type but only combinations of cells.

For these cases Yosys provides the `extract` pass that can match a given set of modules against a design and identify the portions of the design that are identical (i.e. isomorphic subcircuits) to any of the given modules. These matched subcircuits are then replaced by instances of the given modules.

The `extract` pass also finds basic variations of the given modules, such as swapped inputs on commutative cell types.

In addition to this the `extract` pass also has limited support for frequent subcircuit mining, i.e. the process of finding recurring subcircuits in the design. This has a few applications, including the design of new coarse-grain architectures [GW13].

The hard algorithmic work done by the `extract` pass (solving the isomorphic subcircuit problem and frequent subcircuit mining) is performed using the SubCircuit library that can also be used stand-alone without Yosys (see Sec. A.3).

### 9.3 Gate-Level Technology Mapping

On the gate-level the target architecture is usually described by a “Liberty file”. The Liberty file format is an industry standard format that can be used to describe the behaviour and other properties of standard library cells [25].

Mapping a design utilizing the Yosys internal gate library (e.g. as a result of mapping it to this representation using the `techmap` pass) is performed in two phases.

First the register cells must be mapped to the registers that are available on the target architectures. The target architecture might not provide all variations of d-type flip-flops with positive and negative clock edge, high-active and low-active asynchronous set and/or reset, etc. Therefore the process of mapping the registers might add additional inverters to the design and thus it is important to map the register cells first.

Mapping of the register cells may be performed by using the `dfflibmap` pass. This pass expects a Liberty file as argument (using the `-liberty` option) and only uses the register cells from the Liberty file.

Secondly the combinational logic must be mapped to the target architecture. This is done using the external program ABC [27] via the `abc` pass by using the `-liberty` option to the pass. Note that in this case only the combinatorial cells are used from the cell library.

Occasionally Liberty files contain trade secrets (such as sensitive timing information) that cannot be shared freely. This complicates processes such as reporting bugs in the tools involved. When the information in the Liberty file used by Yosys and ABC are not part of the sensitive information, the additional tool `yosys-filterlib` (see Sec. B.2) can be used to strip the sensitive information from the Liberty file.



# Appendix A

## Auxiliary Libraries

The Yosys source distribution contains some auxiliary libraries that are bundled with Yosys.

### A.1 SHA1

The files in `libs/sha1/` provide a public domain SHA1 implementation written by Steve Reid, Bruce Guenter, and Volker Grabsch. It is used for generating unique names when specializing parameterized modules.

### A.2 BigInt

The files in `libs/bigint/` provide a library for performing arithmetic with arbitrary length integers. It is written by Matt McCutchen [29].

The BigInt library is used for evaluating constant expressions, e.g. using the `ConstEval` class provided in `kernel/consteval.h`.

### A.3 SubCircuit

The files in `libs/subcircuit` provide a library for solving the subcircuit isomorphism problem. It is written by Clifford Wolf and based on the Ullmann Subgraph Isomorphism Algorithm [Ull76]. It is used by the `extract` pass (see `help extract` or Sec. C.63).

### A.4 ezSAT

The files in `libs/ezsat` provide a library for simplifying generating CNF formulas for SAT solvers. It also contains bindings of MiniSAT. The ezSAT library is written by Clifford Wolf. It is used by the `sat` pass (see `help sat` or Sec. C.155).

## Appendix B

# Auxiliary Programs

Besides the main `yosys` executable, the Yosys distribution contains a set of additional helper programs.

### B.1 `yosys-config`

The `yosys-config` tool (an auto-generated shell-script) can be used to query compiler options and other information needed for building loadable modules for Yosys. FIXME: See Sec. 6 for details.

### B.2 `yosys-filterlib`

The `yosys-filterlib` tool is a small utility that can be used to strip or extract information from a Liberty file. See Sec. 9.3 for details.

### B.3 `yosys-abc`

This is a fork of ABC [27] with a small set of custom modifications that have not yet been accepted upstream. Not all versions of Yosys work with all versions of ABC. So Yosys comes with its own `yosys-abc` to avoid compatibility issues between the two.

## Appendix C

# Command Reference Manual

### C.1 abc – use ABC for technology mapping

```
1      abc [options] [selection]
2
3  This pass uses the ABC tool [1] for technology mapping of yosys's internal gate
4  library to a target architecture.
5
6  -exe <command>
7      use the specified command instead of "<yosys-bindir>/yosys-abc" to execute ABC.
8      This can e.g. be used to call a specific version of ABC or a wrapper.
9
10 -script <file>
11     use the specified ABC script file instead of the default script.
12
13     if <file> starts with a plus sign (+), then the rest of the filename
14     string is interpreted as the command string to be passed to ABC. The
15     leading plus sign is removed and all commas (,) in the string are
16     replaced with blanks before the string is passed to ABC.
17
18     if no -script parameter is given, the following scripts are used:
19
20     for -liberty without -constr:
21         strash; ifraig; scorr; dc2; dretime; strash; &get -n; &dch -f;
22         &nf {D}; &put
23
24     for -liberty with -constr:
25         strash; ifraig; scorr; dc2; dretime; strash; &get -n; &dch -f;
26         &nf {D}; &put; buffer; upsize {D}; dnsiz {D}; stime -p
27
28     for -lut/-luts (only one LUT size):
29         strash; ifraig; scorr; dc2; dretime; strash; dch -f; if; mfs2;
30         lutpack {S}
31
32     for -lut/-luts (different LUT sizes):
33         strash; ifraig; scorr; dc2; dretime; strash; dch -f; if; mfs2
34
35     for -sop:
```

```

36         strash; ifraig; scorr; dc2; dretime; strash; dch -f;
37         cover {I} {P}
38
39     otherwise:
40         strash; ifraig; scorr; dc2; dretime; strash; &get -n; &dch -f;
41         &nf {D}; &put
42
43 -fast
44     use different default scripts that are slightly faster (at the cost
45     of output quality):
46
47     for -liberty without -constr:
48         strash; dretime; map {D}
49
50     for -liberty with -constr:
51         strash; dretime; map {D}; buffer; upsize {D}; dnsiz {D};
52         stime -p
53
54     for -lut/-luts:
55         strash; dretime; if
56
57     for -sop:
58         strash; dretime; cover -I {I} -P {P}
59
60     otherwise:
61         strash; dretime; map
62
63 -liberty <file>
64     generate netlists for the specified cell library (using the liberty
65     file format).
66
67 -constr <file>
68     pass this file with timing constraints to ABC. use with -liberty.
69
70     a constr file contains two lines:
71         set_driving_cell <cell_name>
72         set_load <floating_point_number>
73
74     the set_driving_cell statement defines which cell type is assumed to
75     drive the primary inputs and the set_load statement sets the load in
76     femtofarads for each primary output.
77
78 -D <picoseconds>
79     set delay target. the string {D} in the default scripts above is
80     replaced by this option when used, and an empty string otherwise.
81     this also replaces 'dretime' with 'dretime; retime -o {D}' in the
82     default scripts above.
83
84 -I <num>
85     maximum number of SOP inputs.
86     (replaces {I} in the default scripts above)
87
88 -P <num>
89     maximum number of SOP products.

```

```

90         (replaces {P} in the default scripts above)
91
92     -S <num>
93         maximum number of LUT inputs shared.
94         (replaces {S} in the default scripts above, default: -S 1)
95
96     -lut <width>
97         generate netlist using luts of (max) the specified width.
98
99     -lut <w1>:<w2>
100         generate netlist using luts of (max) the specified width <w2>. All
101         luts with width <= <w1> have constant cost. for luts larger than <w1>
102         the area cost doubles with each additional input bit. the delay cost
103         is still constant for all lut widths.
104
105     -luts <cost1>,<cost2>,<cost3>,<sizeN>:<cost4-N>,...
106         generate netlist using luts. Use the specified costs for luts with 1,
107         2, 3, .. inputs.
108
109     -sop
110         map to sum-of-product cells and inverters
111
112     -g type1,type2,...
113         Map to the specified list of gate types. Supported gates types are:
114         AND, NAND, OR, NOR, XOR, XNOR, ANDNOT, ORNOT, MUX,
115         NMUX, AOI3, OAI3, AOI4, OAI4.
116         (The NOT gate is always added to this list automatically.)
117
118         The following aliases can be used to reference common sets of gate types:
119         simple: AND OR XOR MUX
120         cmos2:  NAND NOR
121         cmos3:  NAND NOR AOI3 OAI3
122         cmos4:  NAND NOR AOI3 OAI3 AOI4 OAI4
123         cmos:   NAND NOR AOI3 OAI3 AOI4 OAI4 NMUX MUX XOR XNOR
124         gates:  AND NAND OR NOR XOR XNOR ANDNOT ORNOT
125         aig:    AND NAND OR NOR ANDNOT ORNOT
126
127         The alias 'all' represent the full set of all gate types.
128
129         Prefix a gate type with a '-' to remove it from the list. For example
130         the arguments 'AND,OR,XOR' and 'simple,-MUX' are equivalent.
131
132         The default is 'all,-NMUX,-AOI3,-OAI3,-AOI4,-OAI4'.
133
134     -dff
135         also pass $_DFF_?_ and $_DFFE_??_ cells through ABC. modules with many
136         clock domains are automatically partitioned in clock domains and each
137         domain is passed through ABC independently.
138
139     -clk [!]<clock-signal-name>[, [!]<enable-signal-name>]
140         use only the specified clock domain. this is like -dff, but only FF
141         cells that belong to the specified clock domain are used.
142
143     -keepff

```

```

144     set the "keep" attribute on flip-flop output wires. (and thus preserve
145     them, for example for equivalence checking.)
146
147     -nocleanup
148         when this option is used, the temporary files created by this pass
149         are not removed. this is useful for debugging.
150
151     -showtmp
152         print the temp dir name in log. usually this is suppressed so that the
153         command output is identical across runs.
154
155     -markgroups
156         set a 'abcgroupp' attribute on all objects created by ABC. The value of
157         this attribute is a unique integer for each ABC process started. This
158         is useful for debugging the partitioning of clock domains.
159
160     -dress
161         run the 'dress' command after all other ABC commands. This aims to
162         preserve naming by an equivalence check between the original and post-ABC
163         netlists (experimental).
164
165 When neither -liberty nor -lut is used, the Yosys standard cell library is
166 loaded into ABC before the ABC script is executed.
167
168 Note that this is a logic optimization pass within Yosys that is calling ABC
169 internally. This is not going to "run ABC on your design". It will instead run
170 ABC on logic snippets extracted from your design. You will not get any useful
171 output when passing an ABC script that writes a file. Instead write your full
172 design as BLIF file with write_blif and then load that into ABC externally if
173 you want to use ABC to convert your design into another format.
174
175 [1] http://www.eecs.berkeley.edu/~alanmi/abc/

```

## C.2 abc9 – use ABC9 for technology mapping

```

1     abc9 [options] [selection]
2
3 This script pass performs a sequence of commands to facilitate the use of the ABC
4 tool [1] for technology mapping of the current design to a target FPGA
5 architecture. Only fully-selected modules are supported.
6
7     -run <from_label>:<to_label>
8         only run the commands between the labels (see below). an empty
9         from label is synonymous to 'begin', and empty to label is
10        synonymous to the end of the command list.
11
12     -exe <command>
13         use the specified command instead of "<yosys-bindir>/yosys-abc" to execute ABC
14         This can e.g. be used to call a specific version of ABC or a wrapper.
15
16     -script <file>
17         use the specified ABC script file instead of the default script.

```

```

18
19     if <file> starts with a plus sign (+), then the rest of the filename
20     string is interpreted as the command string to be passed to ABC. The
21     leading plus sign is removed and all commas (,) in the string are
22     replaced with blanks before the string is passed to ABC.
23
24     if no -script parameter is given, the following scripts are used:
25         &scorr; &sweep; &dc2; &dch -f; &ps; &if {C} {W} {D} {R} -v; &mfs
26
27 -fast
28     use different default scripts that are slightly faster (at the cost
29     of output quality):
30         &if {C} {W} {D} {R} -v
31
32 -D <picoseconds>
33     set delay target. the string {D} in the default scripts above is
34     replaced by this option when used, and an empty string otherwise
35     (indicating best possible delay).
36
37 -lut <width>
38     generate netlist using luts of (max) the specified width.
39
40 -lut <w1>:<w2>
41     generate netlist using luts of (max) the specified width <w2>. All
42     luts with width <= <w1> have constant cost. for luts larger than <w1>
43     the area cost doubles with each additional input bit. the delay cost
44     is still constant for all lut widths.
45
46 -lut <file>
47     pass this file with lut library to ABC.
48
49 -luts <cost1>,<cost2>,<cost3>,<sizeN>:<cost4-N>,...
50     generate netlist using luts. Use the specified costs for luts with 1,
51     2, 3, .. inputs.
52
53 -maxlut <width>
54     when auto-generating the lut library, discard all luts equal to or
55     greater than this size (applicable when neither -lut nor -luts is
56     specified).
57
58 -dff
59     also pass $_ABC9_FF_ cells through to ABC. modules with many clock
60     domains are marked as such and automatically partitioned by ABC.
61
62 -nocleanup
63     when this option is used, the temporary files created by this pass
64     are not removed. this is useful for debugging.
65
66 -showtmp
67     print the temp dir name in log. usually this is suppressed so that the
68     command output is identical across runs.
69
70 -box <file>
71     pass this file with box library to ABC.

```

Note that this is a logic optimization pass within Yosys that is calling ABC internally. This is not going to "run ABC on your design". It will instead run ABC on logic snippets extracted from your design. You will not get any useful output when passing an ABC script that writes a file. Instead write your full design as an XAIGER file with 'write\_xaiger' and then load that into ABC externally if you want to use ABC to convert your design into another format.

[1] <http://www.eecs.berkeley.edu/~alanmi/abc/>

pre:

```

abc9_ops -check
scc -set_attr abc9_scc_id {}
abc9_ops -mark_scc -prep_delays -prep_xaiger [-dff]      (option for -dff)
abc9_ops -prep_lut <maxlut>      (skip if -lut or -luts)
abc9_ops -prep_box [-dff]      (skip if -box)
select -set abc9_holes A:abc9_holes
flatten -wb @abc9_holes
techmap @abc9_holes
abc9_ops -prep_dff      (only if -dff)
opt -purge @abc9_holes
aigmap
wbflip @abc9_holes

```

map:

```

foreach module in selection
    abc9_ops -write_lut <abc-temp-dir>/input.lut      (skip if '-lut' or '-luts')
    abc9_ops -write_box <abc-temp-dir>/input.box
    write_xaiger -map <abc-temp-dir>/input.sym <abc-temp-dir>/input.xaig
    abc9_exe [options] -cwd <abc-temp-dir> [-lut <abc-temp-dir>/input.lut] -bo
    read_aiger -xaiger -wideports -module_name <module-name>$abc9 -map <abc-te
    abc9_ops -reintegrate

```

### C.3 abc9\_exe – use ABC9 for technology mapping

abc9\_exe [options]

This pass uses the ABC tool [1] for technology mapping of the top module (according to the (\* top \*) attribute or if only one module is currently selected) to a target FPGA architecture.

-exe <command>

use the specified command instead of "<yosys-bindir>/yosys-abc" to execute ABC. This can e.g. be used to call a specific version of ABC or a wrapper.

-script <file>

use the specified ABC script file instead of the default script.

if <file> starts with a plus sign (+), then the rest of the filename string is interpreted as the command string to be passed to ABC. The



leading plus sign is removed and all commas (,) in the string are replaced with blanks before the string is passed to ABC.

if no -script parameter is given, the following scripts are used:  
 &scorr; &sweep; &dc2; &dch -f; &ps; &if {C} {W} {D} {R} -v; &mfs

-fast

use different default scripts that are slightly faster (at the cost of output quality):

&if {C} {W} {D} {R} -v

-D <picoseconds>

set delay target. the string {D} in the default scripts above is replaced by this option when used, and an empty string otherwise (indicating best possible delay).

-lut <width>

generate netlist using luts of (max) the specified width.

-lut <w1>:<w2>

generate netlist using luts of (max) the specified width <w2>. All luts with width <= <w1> have constant cost. for luts larger than <w1> the area cost doubles with each additional input bit. the delay cost is still constant for all lut widths.

-lut <file>

pass this file with lut library to ABC.

-luts <cost1>,<cost2>,<cost3>,<sizeN>:<cost4-N>,...

generate netlist using luts. Use the specified costs for luts with 1, 2, 3, .. inputs.

-showtmp

print the temp dir name in log. usually this is suppressed so that the command output is identical across runs.

-box <file>

pass this file with box library to ABC.

-cwd <dir>

use this as the current working directory, inside which the 'input.xaig' file is expected. temporary files will be created in this directory, and the mapped result will be written to 'output.aig'.

Note that this is a logic optimization pass within Yosys that is calling ABC internally. This is not going to "run ABC on your design". It will instead run ABC on logic snippets extracted from your design. You will not get any useful output when passing an ABC script that writes a file. Instead write your full design as BLIF file with write\_blif and then load that into ABC externally if you want to use ABC to convert your design into another format.

[1] <http://www.eecs.berkeley.edu/~alanmi/abc/>

## C.4 abc9\_ops – helper functions for ABC9

```

1  abc9_ops [options] [selection]
2
3  This pass contains a set of supporting operations for use during ABC technology
4  mapping, and is expected to be called in conjunction with other operations from
5  the 'abc9' script pass. Only fully-selected modules are supported.
6
7  -check
8      check that the design is valid, e.g. (* abc9_box_id *) values are unique,
9      (* abc9_carry *) is only given for one input/output port, etc.
10
11  -prep_delays
12      insert '$_ABC9_DELAY' blackbox cells into the design to account for
13      certain required times.
14
15  -mark_scc
16      for an arbitrarily chosen cell in each unique SCC of each selected module
17      (tagged with an (* abc9_scc_id = <int> *) attribute), temporarily mark all
18      wires driven by this cell's outputs with a (* keep *) attribute in order
19      to break the SCC. this temporary attribute will be removed on -reintegrate.
20
21  -prep_xaiger
22      prepare the design for XAIGER output. this includes computing the
23      topological ordering of ABC9 boxes, as well as preparing the
24      '<module-name>$holes' module that contains the logic behaviour of ABC9
25      whiteboxes.
26
27  -dff
28      consider flop cells (those instantiating modules marked with (* abc9_flop *))
29      during -prep_{delays,xaiger,box}.
30
31  -prep_dff
32      compute the clock domain and initial value of each flop in the design.
33      process the '$holes' module to support clock-enable functionality.
34
35  -prep_lut <maxlut>
36      pre-compute the lut library by analysing all modules marked with
37      (* abc9_lut=<area> *).
38
39  -write_lut <dst>
40      write the pre-computed lut library to <dst>.
41
42  -prep_box
43      pre-compute the box library by analysing all modules marked with
44      (* abc9_box *).
45
46  -write_box <dst>
47      write the pre-computed box library to <dst>.
48
49  -reintegrate
50      for each selected module, re-intergrate the module '<module-name>$abc9'
51      by first recovering ABC9 boxes, and then stitching in the remaining primary
52      inputs and outputs.

```

## C.5 add – add objects to the design

```

1      add <command> [selection]
2
3  This command adds objects to the design. It operates on all fully selected
4  modules. So e.g. 'add -wire foo' will add a wire foo to all selected modules.
5
6
7      add {-wire|-input|-inout|-output} <name> <width> [selection]
8
9  Add a wire (input, inout, output port) with the given name and width. The
10 command will fail if the object exists already and has different properties
11 than the object to be created.
12
13
14      add -global_input <name> <width> [selection]
15
16 Like 'add -input', but also connect the signal between instances of the
17 selected modules.
18
19
20      add {-assert|-assume|-live|-fair|-cover} <name1> [-if <name2>]
21
22 Add an $assert, $assume, etc. cell connected to a wire named name1, with its
23 enable signal optionally connected to a wire named name2 (default: 1'b1).
24
25
26      add -mod <name[s]>
27
28 Add module[s] with the specified name[s].

```

## C.6 aigmap – map logic to and-inverter-graph circuit

```

1      aigmap [options] [selection]
2
3  Replace all logic cells with circuits made of only $_AND_ and
4  $_NOT_ cells.
5
6      -nand
7          Enable creation of $_NAND_ cells
8
9      -select
10         Overwrite replaced cells in the current selection with new $_AND_,
11         $_NOT_, and $_NAND_, cells

```

## C.7 alumacc – extract ALU and MACC cells

```

1      alumacc [selection]
2

```

3 This pass translates arithmetic operations like \$add, \$mul, \$lt, etc. to \$alu  
4 and \$macc cells.

## C.8 anlogic\_eqn – Anlogic: Calculate equations for luts

1 anlogic\_eqn [selection]  
2  
3 Calculate equations for luts since bitstream generator depends on it.

## C.9 anlogic\_fixcarry – Anlogic: fix carry chain

1 anlogic\_fixcarry [options] [selection]  
2  
3 Add Anlogic adders to fix carry chain if needed.

## C.10 assertpmux – adds asserts for parallel muxes

1 assertpmux [options] [selection]  
2  
3 This command adds asserts to the design that assert that all parallel muxes  
4 (\$pmux cells) have a maximum of one of their inputs enable at any time.  
5  
6 -noinit  
7 do not enforce the pmux condition during the init state  
8  
9 -always  
10 usually the \$pmux condition is only checked when the \$pmux output  
11 is used by the mux tree it drives. this option will deactivate this  
12 additional constraint and check the \$pmux condition always.

## C.11 async2sync – convert async FF inputs to sync circuits

1 async2sync [options] [selection]  
2  
3 This command replaces async FF inputs with sync circuits emulating the same  
4 behavior for when the async signals are actually synchronized to the clock.  
5  
6 This pass assumes negative hold time for the async FF inputs. For example when  
7 a reset deasserts with the clock edge, then the FF output will still drive the  
8 reset value in the next cycle regardless of the data-in value at the time of  
9 the clock edge.  
10  
11 Currently only \$adff, \$dffsr, and \$dlatch cells are supported by this pass.

## C.12 attrmap – renaming attributes

```

1  attrmap [options] [selection]
2
3  This command renames attributes and/or maps key/value pairs to
4  other key/value pairs.
5
6  -tocase <name>
7      Match attribute names case-insensitively and set it to the specified
8      name.
9
10 -rename <old_name> <new_name>
11     Rename attributes as specified
12
13 -map <old_name>=<old_value> <new_name>=<new_value>
14     Map key/value pairs as indicated.
15
16 -imap <old_name>=<old_value> <new_name>=<new_value>
17     Like -map, but use case-insensitive match for <old_value> when
18     it is a string value.
19
20 -remove <name>=<value>
21     Remove attributes matching this pattern.
22
23 -modattr
24     Operate on module attributes instead of attributes on wires and cells.
25
26 For example, mapping Xilinx-style "keep" attributes to Yosys-style:
27
28 attrmap -tocase keep -imap keep="true" keep=1 \
29         -imap keep="false" keep=0 -remove keep=0

```

## C.13 attrmvcp – move or copy attributes from wires to driving cells

```

1  attrmvcp [options] [selection]
2
3  Move or copy attributes on wires to the cells driving them.
4
5  -copy
6      By default, attributes are moved. This will only add
7      the attribute to the cell, without removing it from
8      the wire.
9
10 -purge
11     If no selected cell consumes the attribute, then it is
12     left on the wire by default. This option will cause the
13     attribute to be removed from the wire, even if no selected
14     cell takes it.
15
16 -driven
17     By default, attributes are moved to the cell driving the
18     wire. With this option set it will be moved to the cell

```

```

19         driven by the wire instead.
20
21     -attr <attrname>
22         Move or copy this attribute. This option can be used
23         multiple times.

```

## C.14 autaname – automatically assign names to objects

```

1     autaname [selection]
2
3     Assign auto-generated public names to objects with private names (the ones
4     with $-prefix).

```

## C.15 blackbox – convert modules into blackbox modules

```

1     blackbox [options] [selection]
2
3     Convert modules into blackbox modules (remove contents and set the blackbox
4     module attribute).

```

## C.16 bugpoint – minimize testcases

```

1     bugpoint [options]
2
3     This command minimizes testcases that crash Yosys. It removes an arbitrary part
4     of the design and recursively invokes Yosys with a given script, repeating these
5     steps while it can find a smaller design that still causes a crash. Once this
6     command finishes, it replaces the current design with the smallest testcase it
7     was able to produce.
8
9     It is possible to specify the kinds of design part that will be removed. If none
10    are specified, all parts of design will be removed.
11
12    -yosys <filename>
13        use this Yosys binary. if not specified, 'yosys' is used.
14
15    -script <filename>
16        use this script to crash Yosys. required.
17
18    -grep <string>
19        only consider crashes that place this string in the log file.
20
21    -fast
22        run 'proc_clean; clean -purge' after each minimization step. converges
23        faster, but produces larger testcases, and may fail to produce any
24        testcase at all if the crash is related to dangling wires.
25

```

```

26  -clean
27      run 'proc_clean; clean -purge' before checking testcase and after
28      finishing. produces smaller and more useful testcases, but may fail to
29      produce any testcase at all if the crash is related to dangling wires.
30
31  -modules
32      try to remove modules.
33
34  -ports
35      try to remove module ports.
36
37  -cells
38      try to remove cells.
39
40  -connections
41      try to reconnect ports to 'x'.
42
43  -assigns
44      try to remove process assigns from cases.
45
46  -updates
47      try to remove process updates from syncs.

```

### C.17 cd – a shortcut for 'select -module <name>'

```

1      cd <modname>
2
3  This is just a shortcut for 'select -module <modname>'.
4
5
6      cd <cellname>
7
8  When no module with the specified name is found, but there is a cell
9  with the specified name in the current module, then this is equivalent
10 to 'cd <celltype>'.
11
12      cd ..
13
14 Remove trailing substrings that start with '.' in current module name until
15 the name of a module in the current design is generated, then switch to that
16 module. Otherwise clear the current selection.
17
18      cd
19
20 This is just a shortcut for 'select -clear'.

```

### C.18 check – check for obvious problems in the design

```

1      check [options] [selection]
2

```

```

3 This pass identifies the following problems in the current design:
4
5 - combinatorial loops
6
7 - two or more conflicting drivers for one wire
8
9 - used wires that do not have a driver
10
11 Options:
12
13 -noinit
14     Also check for wires which have the 'init' attribute set.
15
16 -initdrv
17     Also check for wires that have the 'init' attribute set and are not
18     driven by an FF cell type.
19
20 -mapped
21     Also check for internal cells that have not been mapped to cells of the
22     target architecture.
23
24 -allow-tbuf
25     Modify the -mapped behavior to still allow $_TBUF_ cells.
26
27 -assert
28     Produce a runtime error if any problems are found in the current design.

```

## C.19 chformal – change formal constraints of the design

```

1     chformal [types] [mode] [options] [selection]
2
3 Make changes to the formal constraints of the design. The [types] options
4 the type of constraint to operate on. If none of the following options are given,
5 the command will operate on all constraint types:
6
7 -assert      $assert cells, representing assert(...) constraints
8 -assume      $assume cells, representing assume(...) constraints
9 -live        $live cells, representing assert(s_eventually ...)
10 -fair        $fair cells, representing assume(s_eventually ...)
11 -cover       $cover cells, representing cover() statements
12
13 Exactly one of the following modes must be specified:
14
15 -remove
16     remove the cells and thus constraints from the design
17
18 -early
19     bypass FFs that only delay the activation of a constraint
20
21 -delay <N>
22     delay activation of the constraint by <N> clock cycles
23

```



```

24     -skip <N>
25         ignore activation of the constraint in the first <N> clock cycles
26
27     -assert2assume
28     -assume2assert
29     -live2fair
30     -fair2live
31         change the roles of cells as indicated. these options can be combined

```

## C.20 chparam – re-evaluate modules with new parameters

```

1     chparam [ -set name value ]... [selection]
2
3     Re-evaluate the selected modules with new parameters. String values must be
4     passed in double quotes (").
5
6
7     chparam -list [selection]
8
9     List the available parameters of the selected modules.

```

## C.21 chtype – change type of cells in the design

```

1     chtype [options] [selection]
2
3     Change the types of cells in the design.
4
5     -set <type>
6         set the cell type to the given type
7
8     -map <old_type> <new_type>
9         change cells types that match <old_type> to <new_type>

```

## C.22 clean – remove unused cells and wires

```

1     clean [options] [selection]
2
3     This is identical to 'opt_clean', but less verbose.
4
5     When commands are separated using the ';;' token, this command will be executed
6     between the commands.
7
8     When commands are separated using the ';;;' token, this command will be executed
9     in -purge mode between the commands.

```

## C.23 clk2fflogic – convert clocked FFs to generic \$ff cells

```

1      clk2fflogic [options] [selection]
2
3  This command replaces clocked flip-flops with generic $ff cells that use the
4  implicit global clock. This is useful for formal verification of designs with
5  multiple clocks.

```

## C.24 clkbufmap – insert global buffers on clock networks

```

1      clkbufmap [options] [selection]
2
3  Inserts global buffers between nets connected to clock inputs and their drivers.
4
5  In the absence of any selection, all wires without the 'clkbuf_inhibit'
6  attribute will be considered for global buffer insertion.
7  Alternatively, to consider all wires without the 'buffer_type' attribute set to
8  'none' or 'bufnr' one would specify:
9      'w:* a:buffer_type=none a:buffer_type=bufnr %u %d'
10 as the selection.
11
12      -buf <celltype> <portname_out>:<portname_in>
13          Specifies the cell type to use for the global buffers
14          and its port names. The first port will be connected to
15          the clock network sinks, and the second will be connected
16          to the actual clock source. This option is required.
17
18      -inpad <celltype> <portname_out>:<portname_in>
19          If specified, a PAD cell of the given type is inserted on
20          clock nets that are also top module's inputs (in addition
21          to the global buffer).

```

## C.25 connect – create or remove connections

```

1      connect [-nomap] [-nounset] -set <lhs-expr> <rhs-expr>
2
3  Create a connection. This is equivalent to adding the statement 'assign
4  <lhs-expr> = <rhs-expr>;' to the Verilog input. Per default, all existing
5  drivers for <lhs-expr> are unconnected. This can be overwritten by using
6  the -nounset option.
7
8
9      connect [-nomap] -unset <expr>
10
11  Unconnect all existing drivers for the specified expression.
12
13
14      connect [-nomap] -port <cell> <port> <expr>
15

```

```

16 Connect the specified cell port to the specified cell port.
17
18
19 Per default signal alias names are resolved and all signal names are mapped
20 the the signal name of the primary driver. Using the -nomap option deactivates
21 this behavior.
22
23 The connect command operates in one module only. Either only one module must
24 be selected or an active module must be set using the 'cd' command.
25
26 This command does not operate on module with processes.

```

## C.26 connect\_rpc – connect to RPC frontend

```

1 connect_rpc -exec <command> [args...]
2 connect_rpc -path <path>
3
4 Load modules using an out-of-process frontend.
5
6 -exec <command> [args...]
7     run <command> with arguments [args...]. send requests on stdin, read
8     responses from stdout.
9
10 -path <path>
11     connect to Unix domain socket at <path>. (Unix)
12     connect to bidirectional byte-type named pipe at <path>. (Windows)
13
14 A simple JSON-based, newline-delimited protocol is used for communicating with
15 the frontend. Yosys requests data from the frontend by sending exactly 1 line
16 of JSON. Frontend responds with data or error message by replying with exactly
17 1 line of JSON as well.
18
19 -> {"method": "modules"}
20 <- {"modules": ["<module-name>", ...]}
21 <- {"error": "<error-message>"}
22     request for the list of modules that can be derived by this frontend.
23     the 'hierarchy' command will call back into this frontend if a cell
24     with type <module-name> is instantiated in the design.
25
26 -> {"method": "derive", "module": "<module-name>", "parameters": {
27     "<param-name>": {"type": "[unsigned|signed|string|real]",
28         "value": "<param-value>"}, ...}}
29 <- {"frontend": "[ilang|verilog|...]", "source": "<source>"}
30 <- {"error": "<error-message>"}
31     request for the module <module-name> to be derived for a specific set of
32     parameters. <param-name> starts with \ for named parameters, and with $
33     for unnamed parameters, which are numbered starting at 1.<param-value>
34     for integer parameters is always specified as a binary string of unlimited
35     precision. the <source> returned by the frontend is hygienically parsed
36     by a built-in Yosys <frontend>, allowing the RPC frontend to return any
37     convenient representation of the module. the derived module is cached,
38     so the response should be the same whenever the same set of parameters

```

39 | is provided.

## C.27 connwrappers – match width of input-output port pairs

```

1   connwrappers [options] [selection]
2
3   Wrappers are used in coarse-grain synthesis to wrap cells with smaller ports
4   in wrapper cells with a (larger) constant port size. I.e. the upper bits
5   of the wrapper output are signed/unsigned bit extended. This command uses this
6   knowledge to rewire the inputs of the driven cells to match the output of
7   the driving cell.
8
9   -signed <cell_type> <port_name> <width_param>
10  -unsigned <cell_type> <port_name> <width_param>
11      consider the specified signed/unsigned wrapper output
12
13  -port <cell_type> <port_name> <width_param> <sign_param>
14      use the specified parameter to decide if signed or unsigned
15
16  The options -signed, -unsigned, and -port can be specified multiple times.
```

## C.28 coolrunner2\_fixup – insert necessary buffer cells for CoolRunner-II architecture

```

1   coolrunner2_fixup [options] [selection]
2
3   Insert necessary buffer cells for CoolRunner-II architecture.
```

## C.29 coolrunner2\_sop – break \$sop cells into ANDTERM/ORTERM cells

```

1   coolrunner2_sop [options] [selection]
2
3   Break $sop cells into ANDTERM/ORTERM cells.
```

## C.30 copy – copy modules in the design

```

1   copy old_name new_name
2
3   Copy the specified module. Note that selection patterns are not supported
4   by this command.
```

### C.31 cover – print code coverage counters

```

1   cover [options] [pattern]
2
3   Print the code coverage counters collected using the cover() macro in the Yosys
4   C++ code. This is useful to figure out what parts of Yosys are utilized by a
5   test bench.
6
7   -q
8       Do not print output to the normal destination (console and/or log file)
9
10  -o file
11      Write output to this file, truncate if exists.
12
13  -a file
14      Write output to this file, append if exists.
15
16  -d dir
17      Write output to a newly created file in the specified directory.
18
19  When one or more pattern (shell wildcards) are specified, then only counters
20  matching at least one pattern are printed.
21
22  It is also possible to instruct Yosys to print the coverage counters on program
23  exit to a file using environment variables:
24
25      YOSYS_COVER_DIR="{dir-name}" yosys {args}
26
27      This will create a file (with an auto-generated name) in this
28      directory and write the coverage counters to it.
29
30      YOSYS_COVER_FILE="{file-name}" yosys {args}
31
32      This will append the coverage counters to the specified file.
33
34  Hint: Use the following AWK command to consolidate Yosys coverage files:
35
36      gawk '{ p[$3] = $1; c[$3] += $2; } END { for (i in p)
37          printf "%-60s %10d %s\n", p[i], c[i], i; }' {files} | sort -k3
38
39
40
41
42  Coverage counters are only available in Yosys for Linux.

```

### C.32 cutpoint – adds formal cut points to the design

```

1   cutpoint [options] [selection]
2
3   This command adds formal cut points to the design.
4
5   -undef

```

```

6      set cupoint nets to undef (x). the default behavior is to create a
7      $anyseq cell and drive the cutpoint net from that

```

### C.33 debug – run command with debug log messages enabled

```

1      debug cmd
2
3  Execute the specified command with debug log messages enabled

```

### C.34 delete – delete objects in the design

```

1      delete [selection]
2
3  Deletes the selected objects. This will also remove entire modules, if the
4  whole module is selected.
5
6
7      delete {-input|-output|-port} [selection]
8
9  Does not delete any object but removes the input and/or output flag on the
10 selected wires, thus 'deleting' module ports.

```

### C.35 deminout – demote inout ports to input or output

```

1      deminout [options] [selection]
2
3  "Demote" inout ports to input or output ports, if possible.

```

### C.36 design – save, restore and reset current design

```

1      design -reset
2
3  Clear the current design.
4
5
6      design -save <name>
7
8  Save the current design under the given name.
9
10
11     design -stash <name>
12
13 Save the current design under the given name and then clear the current design.
14
15

```

```

16     design -push
17
18 Push the current design to the stack and then clear the current design.
19
20
21     design -push-copy
22
23 Push the current design to the stack without clearing the current design.
24
25
26     design -pop
27
28 Reset the current design and pop the last design from the stack.
29
30
31     design -load <name>
32
33 Reset the current design and load the design previously saved under the given
34 name.
35
36
37     design -copy-from <name> [-as <new_mod_name>] <selection>
38
39 Copy modules from the specified design into the current one. The selection is
40 evaluated in the other design.
41
42
43     design -copy-to <name> [-as <new_mod_name>] [selection]
44
45 Copy modules from the current design into the specified one.
46
47
48     design -import <name> [-as <new_top_name>] [selection]
49
50 Import the specified design into the current design. The source design must
51 either have a selected top module or the selection must contain exactly one
52 module that is then used as top module for this command.
53
54
55     design -reset-vlog
56
57 The Verilog front-end remembers defined macros and top-level declarations
58 between calls to 'read_verilog'. This command resets this memory.

```

### C.37 **determine\_init** – Determine the init value of cells

```

1     determine_init [selection]
2
3 Determine the init value of cells that doesn't allow unknown init value.

```

**C.38 dff2dffe – transform \$dff cells to \$dffe cells**

```

1      dff2dffe [options] [selection]
2
3  This pass transforms $dff cells driven by a tree of multiplexers with one or
4  more feedback paths to $dffe cells. It also works on gate-level cells such as
5  $_DFF_P_, $_DFF_N_ and $_MUX_.
6
7  -unmap
8      operate in the opposite direction: replace $dffe cells with combinations
9      of $dff and $mux cells. the options below are ignored in unmap mode.
10
11  -unmap-mince N
12      Same as -unmap but only unmap $dffe where the clock enable port
13      signal is used by less $dffe than the specified number
14
15  -direct <internal_gate_type> <external_gate_type>
16      map directly to external gate type. <internal_gate_type> can
17      be any internal gate-level FF cell (except $_DFFE_??_). the
18      <external_gate_type> is the cell type name for a cell with an
19      identical interface to the <internal_gate_type>, except it
20      also has an high-active enable port 'E'.
21      Usually <external_gate_type> is an intermediate cell type
22      that is then translated to the final type using 'techmap'.
23
24  -direct-match <pattern>
25      like -direct for all DFF cell types matching the expression.
26      this will use $_DFFE_* as <external_gate_type> matching the
27      internal gate type $_DFF_*_, and $_DFFSE_* for those matching
28      $_DFFS_*_, except for $_DFF_[NP]_, which is converted to
29      $_DFFE_[NP]_.

```

**C.39 dff2dffs – process sync set/reset with SR over CE priority**

```

1      dff2dffs [options] [selection]
2
3  Merge synchronous set/reset $_MUX_ cells to create $_DFFS_[NP][NP][01], to be run before
4  dff2dffe for SR over CE priority.
5
6  -match-init
7      Disallow merging synchronous set/reset that has polarity opposite of the
8      output wire's init attribute (if any).

```

**C.40 dffinit – set INIT param on FF cells**

```

1      dffinit [options] [selection]
2
3  This pass sets an FF cell parameter to the the initial value of the net it
4  drives. (This is primarily used in FPGA flows.)

```



```

5
6  -ff <cell_name> <output_port> <init_param>
7      operate on the specified cell type. this option can be used
8      multiple times.
9
10 -highlow
11     use the string values "high" and "low" to represent a single-bit
12     initial value of 1 or 0. (multi-bit values are not supported in this
13     mode.)
14
15 -strinit <string for high> <string for low>
16     use string values in the command line to represent a single-bit
17     initial value of 1 or 0. (multi-bit values are not supported in this
18     mode.)
19
20 -noreinit
21     fail if the FF cell has already a defined initial value set in other
22     passes and the initial value of the net it drives is not equal to
23     the already defined initial value.

```

#### C.41 dfflibmap – technology mapping of flip-flops

```

1  dfflibmap [-prepare] -liberty <file> [selection]
2
3  Map internal flip-flop cells to the flip-flop cells in the technology
4  library specified in the given liberty file.
5
6  This pass may add inverters as needed. Therefore it is recommended to
7  first run this pass and then map the logic paths to the target technology.
8
9  When called with -prepare, this command will convert the internal FF cells
10 to the internal cell types that best match the cells found in the given
11 liberty file.

```

#### C.42 dump – print parts of the design in ilang format

```

1  dump [options] [selection]
2
3  Write the selected parts of the design to the console or specified file in
4  ilang format.
5
6  -m
7      also dump the module headers, even if only parts of a single
8      module is selected
9
10 -n
11     only dump the module headers if the entire module is selected
12
13 -o <filename>
14     write to the specified file.

```

```

15 |
16 |     -a <filename>
17 |         like -outfile but append instead of overwrite

```

### C.43 echo – turning echoing back of commands on and off

```

1 |     echo on
2 |
3 | Print all commands to log before executing them.
4 |
5 |
6 |     echo off
7 |
8 | Do not print all commands to log before executing them. (default)

```

### C.44 ecp5\_ffinit – ECP5: handle FF init values

```

1 |     ecp5_ffinit [options] [selection]
2 |
3 | Remove init values for FF output signals when equal to reset value.
4 | If reset is not used, set the reset value to the init value, otherwise
5 | unmap out the reset (if not an async reset).

```

### C.45 ecp5\_gsr – ECP5: handle GSR

```

1 |     ecp5_gsr [options] [selection]
2 |
3 | Trim active low async resets connected to GSR and resolve GSR parameter,
4 | if a GSR or SGSR primitive is used in the design.
5 |
6 | If any cell has the GSR parameter set to "AUTO", this will be resolved
7 | to "ENABLED" if a GSR primitive is present and the (* nogsr *) attribute
8 | is not set, otherwise it will be resolved to "DISABLED".

```

### C.46 edgetypes – list all types of edges in selection

```

1 |     edgetypes [options] [selection]
2 |
3 | This command lists all unique types of 'edges' found in the selection. An 'edge'
4 | is a 4-tuple of source and sink cell type and port name.

```

**C.47 efinix\_fixcarry – Efinix: fix carry chain**

```

1 efinix_fixcarry [options] [selection]
2
3 Add Efinix adders to fix carry chain if needed.
```

**C.48 efinix\_gbuf – Efinix: insert global clock buffers**

```

1 efinix_gbuf [options] [selection]
2
3 Add Efinix global clock buffers to top module as needed.
```

**C.49 equiv\_add – add a \$equiv cell**

```

1 equiv_add [-try] gold_sig gate_sig
2
3 This command adds an $equiv cell for the specified signals.
4
5
6 equiv_add [-try] -cell gold_cell gate_cell
7
8 This command adds $equiv cells for the ports of the specified cells.
```

**C.50 equiv\_induct – proving \$equiv cells using temporal induction**

```

1 equiv_induct [options] [selection]
2
3 Uses a version of temporal induction to prove $equiv cells.
4
5 Only selected $equiv cells are proven and only selected cells are used to
6 perform the proof.
7
8 -undef
9     enable modelling of undef states
10
11 -seq <N>
12     the max. number of time steps to be considered (default = 4)
13
14 This command is very effective in proving complex sequential circuits, when
15 the internal state of the circuit quickly propagates to $equiv cells.
16
17 However, this command uses a weak definition of 'equivalence': This command
18 proves that the two circuits will not diverge after they produce equal
19 outputs (observable points via $equiv) for at least <N> cycles (the <N>
20 specified via -seq).
21
22 Combined with simulation this is very powerful because simulation can give
```

23 you confidence that the circuits start out synced for at least <N> cycles  
 24 after reset.

### C.51 equiv\_make – prepare a circuit for equivalence checking

```

1     equiv_make [options] gold_module gate_module equiv_module
2
3 This creates a module annotated with $equiv cells from two presumably
4 equivalent modules. Use commands such as 'equiv_simple' and 'equiv_status'
5 to work with the created equivalent checking module.
6
7     -inames
8         Also match cells and wires with $... names.
9
10    -blacklist <file>
11        Do not match cells or signals that match the names in the file.
12
13    -encfile <file>
14        Match FSM encodings using the description from the file.
15        See 'help fsm_recode' for details.
16
17 Note: The circuit created by this command is not a miter (with something like
18 a trigger output), but instead uses $equiv cells to encode the equivalence
19 checking problem. Use 'miter -equiv' if you want to create a miter circuit.
```

### C.52 equiv\_mark – mark equivalence checking regions

```

1     equiv_mark [options] [selection]
2
3 This command marks the regions in an equivalence checking module. Region 0 is
4 the proven part of the circuit. Regions with higher numbers are connected
5 unproven subcircuits. The integer attribute 'equiv_region' is set on all
6 wires and cells.
```

### C.53 equiv\_miter – extract miter from equiv circuit

```

1     equiv_miter [options] miter_module [selection]
2
3 This creates a miter module for further analysis of the selected $equiv cells.
4
5     -trigger
6         Create a trigger output
7
8     -cmp
9         Create cmp_* outputs for individual unproven $equiv cells
10
11    -assert
```

12	Create a \$assert cell for each unproven \$equiv cell
13	
14	-undef
15	Create compare logic that handles undefs correctly

## C.54 equiv\_opt – prove equivalence for optimized circuit

```

1  equiv_opt [options] [command]
2
3  This command uses temporal induction to check circuit equivalence before and
4  after an optimization pass.
5
6  -run <from_label>:<to_label>
7      only run the commands between the labels (see below). an empty
8      from label is synonymous to the start of the command list, and empty to
9      label is synonymous to the end of the command list.
10
11  -map <filename>
12      expand the modules in this file before proving equivalence. this is
13      useful for handling architecture-specific primitives.
14
15  -blacklist <file>
16      Do not match cells or signals that match the names in the file
17      (passed to equiv_make).
18
19  -assert
20      produce an error if the circuits are not equivalent.
21
22  -multiclock
23      run clk2fflogic before equivalence checking.
24
25  -async2sync
26      run async2sync before equivalence checking.
27
28  -undef
29      enable modelling of undef states during equiv_induct.
30
31  The following commands are executed by this verification command:
32
33  run_pass:
34      hierarchy -auto-top
35      design -save preopt
36      [command]
37      design -stash postopt
38
39  prepare:
40      design -copy-from preopt -as gold A:top
41      design -copy-from postopt -as gate A:top
42
43  techmap:    (only with -map)
44      techmap -wb -D EQUIV -autoproc -map <filename> ...
45

```

```

46 prove:
47     clk2fflogic      (only with -multiclock)
48     async2sync      (only with -async2sync)
49     equiv_make -blacklist <filename> ... gold gate equiv
50     equiv_induct [-undef] equiv
51     equiv_status [-assert] equiv
52
53 restore:
54     design -load preopt

```

## C.55 equiv\_purge – purge equivalence checking module

```

1     equiv_purge [options] [selection]
2
3 This command removes the proven part of an equivalence checking module, leaving
4 only the unproven segments in the design. This will also remove and add module
5 ports as needed.

```

## C.56 equiv\_remove – remove \$equiv cells

```

1     equiv_remove [options] [selection]
2
3 This command removes the selected $equiv cells. If neither -gold nor -gate is
4 used then only proven cells are removed.
5
6     -gold
7         keep gold circuit
8
9     -gate
10        keep gate circuit

```

## C.57 equiv\_simple – try proving simple \$equiv instances

```

1     equiv_simple [options] [selection]
2
3 This command tries to prove $equiv cells using a simple direct SAT approach.
4
5     -v
6         verbose output
7
8     -undef
9         enable modelling of undef states
10
11    -short
12        create shorter input cones that stop at shared nodes. This yields
13        simpler SAT problems but sometimes fails to prove equivalence.
14

```

```

15  -nogroup
16      disabling grouping of $equiv cells by output wire
17
18  -seq <N>
19      the max. number of time steps to be considered (default = 1)

```

## C.58 equiv\_status – print status of equivalent checking module

```

1  equiv_status [options] [selection]
2
3  This command prints status information for all selected $equiv cells.
4
5  -assert
6      produce an error if any unproven $equiv cell is found

```

## C.59 equiv\_struct – structural equivalence checking

```

1  equiv_struct [options] [selection]
2
3  This command adds additional $equiv cells based on the assumption that the
4  gold and gate circuit are structurally equivalent. Note that this can introduce
5  bad $equiv cells in cases where the netlists are not structurally equivalent,
6  for example when analyzing circuits with cells with commutative inputs. This
7  command will also de-duplicate gates.
8
9  -fwd
10     by default this command performans forward sweeps until nothing can
11     be merged by forwards sweeps, then backward sweeps until forward
12     sweeps are effective again. with this option set only forward sweeps
13     are performed.
14
15  -fwnonly <cell_type>
16     add the specified cell type to the list of cell types that are only
17     merged in forward sweeps and never in backward sweeps. $equiv is in
18     this list automatically.
19
20  -icells
21     by default, the internal RTL and gate cell types are ignored. add
22     this option to also process those cell types with this command.
23
24  -maxiter <N>
25     maximum number of iterations to run before aborting

```

## C.60 eval – evaluate the circuit given an input

```

1  eval [options] [selection]
2

```

```

3 | This command evaluates the value of a signal given the value of all required
4 | inputs.
5 |
6 |     -set <signal> <value>
7 |         set the specified signal to the specified value.
8 |
9 |     -set-undef
10 |         set all unspecified source signals to undef (x)
11 |
12 |     -table <signal>
13 |         create a truth table using the specified input signals
14 |
15 |     -show <signal>
16 |         show the value for the specified signal. if no -show option is passed
17 |         then all output ports of the current module are used.

```

## C.61 exec – execute commands in the operating system shell

```

1 |     exec [options] -- [command]
2 |
3 | Execute a command in the operating system shell. All supplied arguments are
4 | concatenated and passed as a command to popen(3). Whitespace is not guaranteed
5 | to be preserved, even if quoted. stdin and stderr are not connected, while stdout is
6 | logged unless the "-q" option is specified.
7 |
8 |
9 |     -q
10 |         Suppress stdout and stderr from subprocess
11 |
12 |     -expect-return <int>
13 |         Generate an error if popen() does not return specified value.
14 |         May only be specified once; the final specified value is controlling
15 |         if specified multiple times.
16 |
17 |     -expect-stdout <regex>
18 |         Generate an error if the specified regex does not match any line
19 |         in subprocess's stdout. May be specified multiple times.
20 |
21 |     -not-expect-stdout <regex>
22 |         Generate an error if the specified regex matches any line
23 |         in subprocess's stdout. May be specified multiple times.
24 |
25 |
26 | Example: exec -q -expect-return 0 -- echo "bananapie" | grep "nana"

```

## C.62 expose – convert internal signals to module ports

```

1 |     expose [options] [selection]
2 |
3 | This command exposes all selected internal signals of a module as additional

```



```

4 outputs.
5
6 -dff
7     only consider wires that are directly driven by register cell.
8
9 -cut
10    when exposing a wire, create an input/output pair and cut the internal
11    signal path at that wire.
12
13 -input
14    when exposing a wire, create an input port and disconnect the internal
15    driver.
16
17 -shared
18    only expose those signals that are shared among the selected modules.
19    this is useful for preparing modules for equivalence checking.
20
21 -evert
22    also turn connections to instances of other modules to additional
23    inputs and outputs and remove the module instances.
24
25 -evert-dff
26    turn flip-flops to sets of inputs and outputs.
27
28 -sep <separator>
29    when creating new wire/port names, the original object name is suffixed
30    with this separator (default: '.') and the port name or a type
31    designator for the exposed signal.

```

### C.63 extract – find subcircuits and replace them with cells

```

1  extract -map <map_file> [options] [selection]
2  extract -mine <out_file> [options] [selection]
3
4  This pass looks for subcircuits that are isomorphic to any of the modules
5  in the given map file and replaces them with instances of this modules. The
6  map file can be a Verilog source file (*.v) or an ilang file (*.il).
7
8  -map <map_file>
9      use the modules in this file as reference. This option can be used
10     multiple times.
11
12  -map %<design-name>
13      use the modules in this in-memory design as reference. This option can
14      be used multiple times.
15
16  -verbose
17      print debug output while analyzing
18
19  -constports
20      also find instances with constant drivers. this may be much
21      slower than the normal operation.

```

```

22
23 -nodefaultswaps
24     normally builtin port swapping rules for internal cells are used per
25     default. This turns that off, so e.g. 'a^b' does not match 'b^a'
26     when this option is used.
27
28 -compat <needle_type> <haystack_type>
29     Per default, the cells in the map file (needle) must have the
30     type as the cells in the active design (haystack). This option
31     can be used to register additional pairs of types that should
32     match. This option can be used multiple times.
33
34 -swap <needle_type> <port1>,<port2>[,...]
35     Register a set of swappable ports for a needle cell type.
36     This option can be used multiple times.
37
38 -perm <needle_type> <port1>,<port2>[,...] <portA>,<portB>[,...]
39     Register a valid permutation of swappable ports for a needle
40     cell type. This option can be used multiple times.
41
42 -cell_attr <attribute_name>
43     Attributes on cells with the given name must match.
44
45 -wire_attr <attribute_name>
46     Attributes on wires with the given name must match.
47
48 -ignore_parameters
49     Do not use parameters when matching cells.
50
51 -ignore_param <cell_type> <parameter_name>
52     Do not use this parameter when matching cells.
53
54 This pass does not operate on modules with unprocessed processes in it.
55 (I.e. the 'proc' pass should be used first to convert processes to netlists.)
56
57 This pass can also be used for mining for frequent subcircuits. In this mode
58 the following options are to be used instead of the -map option.
59
60 -mine <out_file>
61     mine for frequent subcircuits and write them to the given ilang file
62
63 -mine_cells_span <min> <max>
64     only mine for subcircuits with the specified number of cells
65     default value: 3 5
66
67 -mine_min_freq <num>
68     only mine for subcircuits with at least the specified number of matches
69     default value: 10
70
71 -mine_limit_matches_per_module <num>
72     when calculating the number of matches for a subcircuit, don't count
73     more than the specified number of matches per module
74
75 -mine_max_fanout <num>

```

```

76         don't consider internal signals with more than <num> connections
77
78 The modules in the map file may have the attribute 'extract_order' set to an
79 integer value. Then this value is used to determine the order in which the pass
80 tries to map the modules to the design (ascending, default value is 0).
81
82 See 'help techmap' for a pass that does the opposite thing.

```

## C.64 `extract_counter` – Extract GreenPak4 counter cells

```

1  extract_counter [options] [selection]
2
3  This pass converts non-resettable or async resettable down counters to
4  counter cells. Use a target-specific 'techmap' map file to convert those cells
5  to the actual target cells.
6
7  -maxwidth N
8      Only extract counters up to N bits wide (default 64)
9
10 -minwidth N
11     Only extract counters at least N bits wide (default 2)
12
13 -allow_arst yes|no
14     Allow counters to have async reset (default yes)
15
16 -dir up|down|both
17     Look for up-counters, down-counters, or both (default down)
18
19 -pout X,Y,...
20     Only allow parallel output from the counter to the listed cell types
21     (if not specified, parallel outputs are not restricted)

```

## C.65 `extract_fa` – find and extract full/half adders

```

1  extract_fa [options] [selection]
2
3  This pass extracts full/half adders from a gate-level design.
4
5  -fa, -ha
6      Enable cell types (fa=full adder, ha=half adder)
7      All types are enabled if none of this options is used
8
9  -d <int>
10     Set maximum depth for extracted logic cones (default=20)
11
12 -b <int>
13     Set maximum breadth for extracted logic cones (default=6)
14
15 -v
16     Verbose output

```

**C.66 extract\_reduce – converts gate chains into \$reduce\_\* cells**

```

1      extract_reduce [options] [selection]
2
3  converts gate chains into $reduce_* cells
4
5  This command finds chains of $_AND_, $_OR_, and $_XOR_ cells and replaces them
6  with their corresponding $reduce_* cells. Because this command only operates on
7  these cell types, it is recommended to map the design to only these cell types
8  using the 'abc -g' command. Note that, in some cases, it may be more effective
9  to map the design to only $_AND_ cells, run extract_reduce, map the remaining
10 parts of the design to AND/OR/XOR cells, and run extract_reduce a second time.
11
12      -allow-off-chain
13          Allows matching of cells that have loads outside the chain. These cells
14          will be replicated and folded into the $reduce_* cell, but the original
15          cell will remain, driving its original loads.

```

**C.67 extractinv – extract explicit inverter cells for invertible cell pins**

```

1      extractinv [options] [selection]
2
3  Searches the design for all cells with invertible pins controlled by a cell
4  parameter (eg. IS_CLK_INVERTED on many Xilinx cells) and removes the parameter.
5  If the parameter was set to 1, inserts an explicit inverter cell in front of
6  the pin instead. Normally used for output to ISE, which does not support the
7  inversion parameters.
8
9  To mark a cell port as invertible, use (* invertible_pin = "param_name" *)
10 on the wire in the blackbox module. The parameter value should have
11 the same width as the port, and will be effectively XORed with it.
12
13      -inv <celltype> <portname_out>:<portname_in>
14          Specifies the cell type to use for the inverters and its port names.
15          This option is required.

```

**C.68 flatten – flatten design**

```

1      flatten [options] [selection]
2
3  This pass flattens the design by replacing cells by their implementation. This
4  pass is very similar to the 'techmap' pass. The only difference is that this
5  pass is using the current design as mapping library.
6
7  Cells and/or modules with the 'keep_hierarchy' attribute set will not be
8  flattened by this command.
9
10      -wb
11          Ignore the 'whitebox' attribute on cell implementations.

```

**C.69 flowmap – pack LUTs with FlowMap**

```

1  flowmap [options] [selection]
2
3  This pass uses the FlowMap technology mapping algorithm to pack logic gates
4  into k-LUTs with optimal depth. It allows mapping any circuit elements that can
5  be evaluated with the 'eval' pass, including cells with multiple output ports
6  and multi-bit input and output ports.
7
8  -maxlut k
9      perform technology mapping for a k-LUT architecture. if not specified,
10     defaults to 3.
11
12  -minlut n
13     only produce n-input or larger LUTs. if not specified, defaults to 1.
14
15  -cells <cell>[,<cell>,...]
16     map specified cells. if not specified, maps $_NOT_, $_AND_, $_OR_,
17     $_XOR_ and $_MUX_, which are the outputs of the 'simplemap' pass.
18
19  -relax
20     perform depth relaxation and area minimization.
21
22  -r-alpha n, -r-beta n, -r-gamma n
23     parameters of depth relaxation heuristic potential function.
24     if not specified, alpha=8, beta=2, gamma=1.
25
26  -optarea n
27     optimize for area by trading off at most n logic levels for fewer LUTs.
28     n may be zero, to optimize for area without increasing depth.
29     implies -relax.
30
31  -debug
32     dump intermediate graphs.
33
34  -debug-relax
35     explain decisions performed during depth relaxation.

```

**C.70 fmcombine – combine two instances of a cell into one**

```

1  fmcombine [options] module_name gold_cell gate_cell
2
3  This pass takes two cells, which are instances of the same module, and replaces
4  them with one instance of a special 'combined' module, that effectively
5  contains two copies of the original module, plus some formal properties.
6
7  This is useful for formal test benches that check what differences in behavior
8  a slight difference in input causes in a module.
9
10  -initeq
11     Insert assumptions that initially all FFs in both circuits have the
12     same initial values.

```

```

13
14 -anyeq
15     Do not duplicate $anyseq/$anyconst cells.
16
17 -fwd
18     Insert forward hint assumptions into the combined module.
19
20 -bwd
21     Insert backward hint assumptions into the combined module.
22     (Backward hints are logically equivalent to forward hits, but
23     some solvers are faster with bwd hints, or even both -bwd and -fwd.)
24
25 -nop
26     Don't insert hint assumptions into the combined module.
27     (This should not provide any speedup over the original design, but
28     strangely sometimes it does.)
29
30 If none of -fwd, -bwd, and -nop is given, then -fwd is used as default.

```

### C.71 fminit – set init values/sequences for formal

```

1     fminit [options] <selection>
2
3 This pass creates init constraints (for example for reset sequences) in a formal
4 model.
5
6 -seq <signal> <sequence>
7     Set sequence using comma-separated list of values, use 'z for
8     unconstrained bits. The last value is used for the remainder of the
9     trace.
10
11 -set <signal> <value>
12     Add constant value constraint
13
14 -posedge <signal>
15 -negedge <signal>
16     Set clock for init sequences

```

### C.72 freduce – perform functional reduction

```

1     freduce [options] [selection]
2
3 This pass performs functional reduction in the circuit. I.e. if two nodes are
4 equivalent, they are merged to one node and one of the redundant drivers is
5 disconnected. A subsequent call to 'clean' will remove the redundant drivers.
6
7 -v, -vv
8     enable verbose or very verbose output
9
10 -inv

```

```

11         enable explicit handling of inverted signals
12
13     -stop <n>
14         stop after <n> reduction operations. this is mostly used for
15         debugging the freduce command itself.
16
17     -dump <prefix>
18         dump the design to <prefix>_<module>_<num>.il after each reduction
19         operation. this is mostly used for debugging the freduce command.
20
21 This pass is undef-aware, i.e. it considers don't-care values for detecting
22 equivalent nodes.
23
24 All selected wires are considered for rewiring. The selected cells cover the
25 circuit that is analyzed.

```

### C.73 fsm – extract and optimize finite state machines

```

1     fsm [options] [selection]
2
3 This pass calls all the other fsm_* passes in a useful order. This performs
4 FSM extraction and optimization. It also calls opt_clean as needed:
5
6     fsm_detect           unless got option -nodetect
7     fsm_extract
8
9     fsm_opt
10    opt_clean
11    fsm_opt
12
13    fsm_expand           if got option -expand
14    opt_clean            if got option -expand
15    fsm_opt              if got option -expand
16
17    fsm_recode           unless got option -norecode
18
19    fsm_info
20
21    fsm_export           if got option -export
22    fsm_map              unless got option -nomap
23
24 Options:
25
26    -expand, -norecode, -export, -nomap
27        enable or disable passes as indicated above
28
29    -fullexpand
30        call expand with -full option
31
32    -encoding type
33    -fm_set_fsm_file file
34    -encfile file

```

35 | passed through to fsm\_recode pass

## C.74 fsm\_detect – finding FSMs in design

```

1   fsm_detect [selection]
2
3   This pass detects finite state machines by identifying the state signal.
4   The state signal is then marked by setting the attribute 'fsm_encoding'
5   on the state signal to "auto".
6
7   Existing 'fsm_encoding' attributes are not changed by this pass.
8
9   Signals can be protected from being detected by this pass by setting the
10  'fsm_encoding' attribute to "none".

```

## C.75 fsm\_expand – expand FSM cells by merging logic into it

```

1   fsm_expand [-full] [selection]
2
3   The fsm_extract pass is conservative about the cells that belong to a finite
4   state machine. This pass can be used to merge additional auxiliary gates into
5   the finite state machine.
6
7   By default, fsm_expand is still a bit conservative regarding merging larger
8   word-wide cells. Call with -full to consider all cells for merging.

```

## C.76 fsm\_export – exporting FSMs to KISS2 files

```

1   fsm_export [-noauto] [-o filename] [-origenc] [selection]
2
3   This pass creates a KISS2 file for every selected FSM. For FSMs with the
4   'fsm_export' attribute set, the attribute value is used as filename, otherwise
5   the module and cell name is used as filename. If the parameter '-o' is given,
6   the first exported FSM is written to the specified filename. This overwrites
7   the setting as specified with the 'fsm_export' attribute. All other FSMs are
8   exported to the default name as mentioned above.
9
10  -noauto
11      only export FSMs that have the 'fsm_export' attribute set
12
13  -o filename
14      filename of the first exported FSM
15
16  -origenc
17      use binary state encoding as state names instead of s0, s1, ...

```



**C.77 fsm\_extract – extracting FSMs in design**

```

1      fsm_extract [selection]
2
3  This pass operates on all signals marked as FSM state signals using the
4  'fsm_encoding' attribute. It consumes the logic that creates the state signal
5  and uses the state signal to generate control signal and replaces it with an
6  FSM cell.
7
8  The generated FSM cell still generates the original state signal with its
9  original encoding. The 'fsm_opt' pass can be used in combination with the
10 'opt_clean' pass to eliminate this signal.

```

**C.78 fsm\_info – print information on finite state machines**

```

1      fsm_info [selection]
2
3  This pass dumps all internal information on FSM cells. It can be useful for
4  analyzing the synthesis process and is called automatically by the 'fsm'
5  pass so that this information is included in the synthesis log file.

```

**C.79 fsm\_map – mapping FSMs to basic logic**

```

1      fsm_map [selection]
2
3  This pass translates FSM cells to flip-flops and logic.

```

**C.80 fsm\_opt – optimize finite state machines**

```

1      fsm_opt [selection]
2
3  This pass optimizes FSM cells. It detects which output signals are actually
4  not used and removes them from the FSM. This pass is usually used in
5  combination with the 'opt_clean' pass (see also 'help fsm').

```

**C.81 fsm\_recode – recoding finite state machines**

```

1      fsm_recode [options] [selection]
2
3  This pass reassign the state encodings for FSM cells. At the moment only
4  one-hot encoding and binary encoding is supported.
5      -encoding <type>
6          specify the encoding scheme used for FSMs without the
7          'fsm_encoding' attribute or with the attribute set to 'auto'.

```

```

8
9  -fm_set_fsm_file <file>
10      generate a file containing the mapping from old to new FSM encoding
11      in form of Synopsys Formality set_fsm_* commands.
12
13  -encfile <file>
14      write the mappings from old to new FSM encoding to a file in the
15      following format:
16
17          .fsm <module_name> <state_signal>
18          .map <old_bitpattern> <new_bitpattern>

```

## C.82 greenpak4\_dffinv – merge greenpak4 inverters and DFF/latches

```

1  greenpak4_dffinv [options] [selection]
2
3  Merge GP_INV cells with GP_DFF* and GP_DLATCH* cells.

```

## C.83 help – display help messages

```

1  help ..... list all commands
2  help <command> ..... print help message for given command
3  help -all ..... print complete command reference
4
5  help -cells ..... list all cell types
6  help <celltype> ..... print help message for given cell type
7  help <celltype>+ .... print verilog code for given cell type

```

## C.84 hierarchy – check, expand and clean up design hierarchy

```

1  hierarchy [-check] [-top <module>]
2  hierarchy -generate <cell-types> <port-decls>
3
4  In parametric designs, a module might exist in several variations with
5  different parameter values. This pass looks at all modules in the current
6  design and re-runs the language frontends for the parametric modules as
7  needed. It also resolves assignments to wired logic data types (wand/wor),
8  resolves positional module parameters, unroll array instances, and more.
9
10  -check
11      also check the design hierarchy. this generates an error when
12      an unknown module is used as cell type.
13
14  -simcheck
15      like -check, but also throw an error if blackbox modules are
16      instantiated, and throw an error if the design has no top module.
17

```

```

18  -purge_lib
19      by default the hierarchy command will not remove library (blackbox)
20      modules. use this option to also remove unused blackbox modules.
21
22  -libdir <directory>
23      search for files named <module_name>.v in the specified directory
24      for unknown modules and automatically run read_verilog for each
25      unknown module.
26
27  -keep_positionals
28      per default this pass also converts positional arguments in cells
29      to arguments using port names. This option disables this behavior.
30
31  -keep_portwidths
32      per default this pass adjusts the port width on cells that are
33      module instances when the width does not match the module port. This
34      option disables this behavior.
35
36  -nodefaults
37      do not resolve input port default values
38
39  -nokeep_asserts
40      per default this pass sets the "keep" attribute on all modules
41      that directly or indirectly contain one or more formal properties.
42      This option disables this behavior.
43
44  -top <module>
45      use the specified top module to build the design hierarchy. Modules
46      outside this tree (unused modules) are removed.
47
48      when the -top option is used, the 'top' attribute will be set on the
49      specified top module. otherwise a module with the 'top' attribute set
50      will implicitly be used as top module, if such a module exists.
51
52  -auto-top
53      automatically determine the top of the design hierarchy and mark it.
54
55  -chparam name value
56      elaborate the top module using this parameter value. Modules on which
57      this parameter does not exist may cause a warning message to be output.
58      This option can be specified multiple times to override multiple
59      parameters. String values must be passed in double quotes (").
60
61  In -generate mode this pass generates blackbox modules for the given cell
62  types (wildcards supported). For this the design is searched for cells that
63  match the given types and then the given port declarations are used to
64  determine the direction of the ports. The syntax for a port declaration is:
65
66      {i|o|io}[@<num>]:<portname>
67
68  Input ports are specified with the 'i' prefix, output ports with the 'o'
69  prefix and inout ports with the 'io' prefix. The optional <num> specifies
70  the position of the port in the parameter list (needed when instantiated
71  using positional arguments). When <num> is not specified, the <portname> can

```

```

72 | also contain wildcard characters.
73 |
74 | This pass ignores the current selection and always operates on all modules
75 | in the current design.

```

## C.85 hilomap – technology mapping of constant hi- and/or lo-drivers

```

1 |     hilomap [options] [selection]
2 |
3 | Map constants to 'tielo' and 'tiehi' driver cells.
4 |
5 |     -hicell <celltype> <portname>
6 |         Replace constant hi bits with this cell.
7 |
8 |     -locell <celltype> <portname>
9 |         Replace constant lo bits with this cell.
10 |
11 |     -singleton
12 |         Create only one hi/lo cell and connect all constant bits
13 |         to that cell. Per default a separate cell is created for
14 |         each constant bit.

```

## C.86 history – show last interactive commands

```

1 |     history
2 |
3 | This command prints all commands in the shell history buffer. This are
4 | all commands executed in an interactive session, but not the commands
5 | from executed scripts.

```

## C.87 ice40\_braminit – iCE40: perform SB\_RAM40\_4K initialization from file

```

1 |     ice40_braminit
2 |
3 | This command processes all SB_RAM40_4K blocks with a non-empty INIT_FILE
4 | parameter and converts it into the required INIT_x attributes

```

## C.88 ice40\_dsp – iCE40: map multipliers

```

1 |     ice40_dsp [options] [selection]
2 |
3 | Map multipliers ($mul/SB_MAC16) and multiply-accumulate ($mul/SB_MAC16 + $add)
4 | cells into iCE40 DSP resources.

```

```

5 | Currently, only the 16x16 multiply mode is supported and not the 2 x 8x8 mode.
6 |
7 | Pack input registers (A, B, {C,D}); with optional hold), pipeline registers
8 | ({F,J,K,G}, H), output registers (O -- full 32-bits or lower 16-bits only; with
9 | optional hold), and post-adder into the SB_MAC16 resource.
10 |
11 | Multiply-accumulate operations using the post-adder with feedback on the {C,D}
12 | input will be folded into the DSP. In this scenario only, resetting the
13 | the accumulator to an arbitrary value can be inferred to use the {C,D} input.

```

### C.89 ice40\_ffinit – iCE40: handle FF init values

```

1 | ice40_ffinit [options] [selection]
2 |
3 | Remove zero init values for FF output signals. Add inverters to implement
4 | nonzero init values.

```

### C.90 ice40\_ffssr – iCE40: merge synchronous set/reset into FF cells

```

1 | ice40_ffssr [options] [selection]
2 |
3 | Merge synchronous set/reset $_MUX_ cells into iCE40 FFs.

```

### C.91 ice40\_opt – iCE40: perform simple optimizations

```

1 | ice40_opt [options] [selection]
2 |
3 | This command executes the following script:
4 |
5 |     do
6 |         <ice40 specific optimizations>
7 |         opt_expr -mux_undef -undriven [-full]
8 |         opt_merge
9 |         opt_rmdff
10 |        opt_clean
11 |    while <changed design>

```

### C.92 ice40\_wrapcarry – iCE40: wrap carries

```

1 | ice40_wrapcarry [selection]
2 |
3 | Wrap manually instantiated SB_CARRY cells, along with their associated SB_LUT4s,
4 | into an internal $__ICE40_CARRY_WRAPPER cell for preservation across technology
5 | mapping.
6 |

```

```

7 Attributes on both cells will have their names prefixed with 'SB_CARRY.' or
8 'SB_LUT4.' and attached to the wrapping cell.
9 A (* keep *) attribute on either cell will be logically OR-ed together.
10
11     -unwrap
12         unwrap $__ICE40_CARRY_WRAPPER cells back into SB_CARRYs and SB_LUT4s,
13         including restoring their attributes.

```

### C.93 insbuf – insert buffer cells for connected wires

```

1     insbuf [options] [selection]
2
3 Insert buffer cells into the design for directly connected wires.
4
5     -buf <celltype> <in-portname> <out-portname>
6         Use the given cell type instead of $_BUF_. (Notice that the next
7         call to "clean" will remove all $_BUF_ in the design.)

```

### C.94 iopadmap – technology mapping of i/o pads (or buffers)

```

1     iopadmap [options] [selection]
2
3 Map module inputs/outputs to PAD cells from a library. This pass
4 can only map to very simple PAD cells. Use 'techmap' to further map
5 the resulting cells to more sophisticated PAD cells.
6
7     -inpad <celltype> <portname>[:<portname>]
8         Map module input ports to the given cell type with the
9         given output port name. if a 2nd portname is given, the
10        signal is passed through the pad call, using the 2nd
11        portname as the port facing the module port.
12
13     -outpad <celltype> <portname>[:<portname>]
14     -inoutpad <celltype> <portname>[:<portname>]
15         Similar to -inpad, but for output and inout ports.
16
17     -toutpad <celltype> <portname>:<portname>[:<portname>]
18         Merges $_TBUF_ cells into the output pad cell. This takes precedence
19         over the other -outpad cell. The first portname is the enable input
20         of the tristate driver.
21
22     -tinoutpad <celltype> <portname>:<portname>:<portname>[:<portname>]
23         Merges $_TBUF_ cells into the inout pad cell. This takes precedence
24         over the other -inoutpad cell. The first portname is the enable input
25         of the tristate driver and the 2nd portname is the internal output
26         buffering the external signal.
27
28     -ignore <celltype> <portname>[:<portname>]*
29         Skips mapping inputs/outputs that are already connected to given
30         ports of the given cell. Can be used multiple times. This is in

```

```

31      addition to the cells specified as mapping targets.
32
33      -widthparam <param_name>
34          Use the specified parameter name to set the port width.
35
36      -nameparam <param_name>
37          Use the specified parameter to set the port name.
38
39      -bits
40          create individual bit-wide buffers even for ports that
41          are wider. (the default behavior is to create word-wide
42          buffers using -widthparam to set the word size on the cell.)
43
44      Tristate PADS (-toutpad, -tinoutpad) always operate in -bits mode.

```

## C.95 json – write design in JSON format

```

1      json [options] [selection]
2
3      Write a JSON netlist of all selected objects.
4
5      -o <filename>
6          write to the specified file.
7
8      -aig
9          also include AIG models for the different gate types
10
11     -compat-int
12         emit 32-bit or smaller fully-defined parameter values directly
13         as JSON numbers (for compatibility with old parsers)
14
15     See 'help write_json' for a description of the JSON format used.

```

## C.96 log – print text and log files

```

1      log string
2
3      Print the given string to the screen and/or the log file. This is useful for TCL
4      scripts, because the TCL command "puts" only goes to stdout but not to
5      logfiles.
6
7      -stdout
8          Print the output to stdout too. This is useful when all Yosys is executed
9          with a script and the -q (quiet operation) argument to notify the user.
10
11     -stderr
12         Print the output to stderr too.
13
14     -nolog
15         Don't use the internal log() command. Use either -stdout or -stderr,

```

```

16         otherwise no output will be generated at all.
17
18     -n
19         do not append a newline

```

## C.97 logger – set logger properties

```

1     logger [options]
2
3     This command sets global logger properties, also available using command line
4     options.
5
6     -[no]time
7         enable/disable display of timestamp in log output.
8
9     -[no]stderr
10        enable/disable logging errors to stderr.
11
12     -warn regex
13        print a warning for all log messages matching the regex.
14
15     -nowarn regex
16        if a warning message matches the regex, it is printed as regular
17        message instead.
18
19     -werror regex
20        if a warning message matches the regex, it is printed as error
21        message instead and the tool terminates with a nonzero return code.
22
23     -[no]debug
24        globally enable/disable debug log messages.
25
26     -experimental <feature>
27        do not print warnings for the specified experimental feature
28
29     -expect <type> <regex> <expected_count>
30        expect log,warning or error to appear. In case of error return code is 0.
31
32     -expect-no-warnings
33        gives error in case there is at least one warning that is not expected.

```

## C.98 ls – list modules or objects in modules

```

1     ls [selection]
2
3     When no active module is selected, this prints a list of modules.
4
5     When an active module is selected, this prints a list of objects in the module.

```



**C.99 ltp – print longest topological path**

```

1      ltp [options] [selection]
2
3  This command prints the longest topological path in the design. (Only considers
4  paths within a single module, so the design must be flattened.)
5
6      -noff
7          automatically exclude FF cell types

```

**C.100 lut2mux – convert \$lut to \$\_MUX\_**

```

1      lut2mux [options] [selection]
2
3  This pass converts $lut cells to $_MUX_ gates.

```

**C.101 maccmap – mapping macc cells**

```

1      maccmap [-unmap] [selection]
2
3  This pass maps $macc cells to yosys $fa and $alu cells. When the -unmap option
4  is used then the $macc cell is mapped to $add, $sub, etc. cells instead.

```

**C.102 memory – translate memories to basic cells**

```

1      memory [-nomap] [-nordff] [-memx] [-bram <bram_rules>] [selection]
2
3  This pass calls all the other memory_* passes in a useful order:
4
5      opt_mem
6      memory_dff [-nordff]                (-memx implies -nordff)
7      opt_clean
8      memory_share
9      opt_clean
10     memory_memx                        (when called with -memx)
11     memory_collect
12     memory_bram -rules <bram_rules>    (when called with -bram)
13     memory_map                        (skipped if called with -nomap)
14
15  This converts memories to word-wide DFFs and address decoders
16  or multiport memory blocks if called with the -nomap option.

```

**C.103 memory\_bram – map memories to block rams**

```

1  memory_bram -rules <rule_file> [selection]
2
3  This pass converts the multi-port $mem memory cells into block ram instances.
4  The given rules file describes the available resources and how they should be
5  used.
6
7  The rules file contains configuration options, a set of block ram description
8  and a sequence of match rules.
9
10 The option 'attr_icase' configures how attribute values are matched. The value 0
11 means case-sensitive, 1 means case-insensitive.
12
13 A block ram description looks like this:
14
15     bram RAMB1024X32      # name of BRAM cell
16     init 1                # set to '1' if BRAM can be initialized
17     abits 10              # number of address bits
18     dbits 32              # number of data bits
19     groups 2              # number of port groups
20     ports 1 1             # number of ports in each group
21     wrmode 1 0            # set to '1' if this groups is write ports
22     enable 4 1            # number of enable bits
23     transp 0 2            # transparent (for read ports)
24     clocks 1 2            # clock configuration
25     clkpol 2 2            # clock polarity configuration
26     endbram
27
28 For the option 'transp' the value 0 means non-transparent, 1 means transparent
29 and a value greater than 1 means configurable. All groups with the same
30 value greater than 1 share the same configuration bit.
31
32 For the option 'clocks' the value 0 means non-clocked, and a value greater
33 than 0 means clocked. All groups with the same value share the same clock
34 signal.
35
36 For the option 'clkpol' the value 0 means negative edge, 1 means positive edge
37 and a value greater than 1 means configurable. All groups with the same value
38 greater than 1 share the same configuration bit.
39
40 Using the same bram name in different bram blocks will create different variants
41 of the bram. Verilog configuration parameters for the bram are created as needed.
42
43 It is also possible to create variants by repeating statements in the bram block
44 and appending '@<label>' to the individual statements.
45
46 A match rule looks like this:
47
48     match RAMB1024X32
49         max waste 16384    # only use this bram if <= 16k ram bits are unused
50         min efficiency 80  # only use this bram if efficiency is at least 80%
51     endmatch
52

```

```

53 It is possible to match against the following values with min/max rules:
54
55 words ..... number of words in memory in design
56 abits ..... number of address bits on memory in design
57 dbits ..... number of data bits on memory in design
58 wports ..... number of write ports on memory in design
59 rports ..... number of read ports on memory in design
60 ports ..... number of ports on memory in design
61 bits ..... number of bits in memory in design
62 dups ..... number of duplications for more read ports
63
64 awaste ..... number of unused address slots for this match
65 dwaste ..... number of unused data bits for this match
66 bwaste ..... number of unused bram bits for this match
67 waste ..... total number of unused bram bits (bwaste*dups)
68 efficiency ... total percentage of used and non-duplicated bits
69
70 acells ..... number of cells in 'address-direction'
71 dcells ..... number of cells in 'data-direction'
72 cells ..... total number of cells (acells*dcells*dups)
73
74 A match containing the command 'attribute' followed by a list of space
75 separated 'name[=string_value]' values requires that the memory contains any
76 one of the given attribute name and string values (where specified), or name
77 and integer 1 value (if no string_value given, since Verilog will interpret
78 '(* attr *)' as '(* attr=1 *)').
79 A name prefixed with '!' indicates that the attribute must not exist.
80
81 The interface for the created bram instances is derived from the bram
82 description. Use 'techmap' to convert the created bram instances into
83 instances of the actual bram cells of your target architecture.
84
85 A match containing the command 'or_next_if_better' is only used if it
86 has a higher efficiency than the next match (and the one after that if
87 the next also has 'or_next_if_better' set, and so forth).
88
89 A match containing the command 'make_transp' will add external circuitry
90 to simulate 'transparent read', if necessary.
91
92 A match containing the command 'make_outreg' will add external flip-flops
93 to implement synchronous read ports, if necessary.
94
95 A match containing the command 'shuffle_enable A' will re-organize
96 the data bits to accommodate the enable pattern of port A.

```

## C.104 memory\_collect – creating multi-port memory cells

```

1 memory_collect [selection]
2
3 This pass collects memories and memory ports and creates generic multiport
4 memory cells.

```

**C.105 memory\_dff – merge input/output DFFs into memories**

```

1  memory_dff [options] [selection]
2
3  This pass detects DFFs at memory ports and merges them into the memory port.
4  I.e. it consumes an asynchronous memory port and the flip-flops at its
5  interface and yields a synchronous memory port.
6
7  -nordfff
8      do not merge registers on read ports

```

**C.106 memory\_map – translate multiport memories to basic cells**

```

1  memory_map [options] [selection]
2
3  This pass converts multiport memory cells as generated by the memory_collect
4  pass to word-wide DFFs and address decoders.
5
6  -attr !<name>
7      do not map memories that have attribute <name> set.
8
9  -attr <name>[=<value>]
10     for memories that have attribute <name> set, only map them if its value
11     is a string <value> (if specified), or an integer 1 (otherwise). if this
12     option is specified multiple times, map the memory if the attribute is
13     to any of the values.
14
15  -iattr
16     for -attr, ignore case of <value>.

```

**C.107 memory\_memx – emulate vlog sim behavior for mem ports**

```

1  memory_memx [selection]
2
3  This pass adds additional circuitry that emulates the Verilog simulation
4  behavior for out-of-bounds memory reads and writes.

```

**C.108 memory\_nordff – extract read port FFs from memories**

```

1  memory_nordff [options] [selection]
2
3  This pass extracts FFs from memory read ports. This results in a netlist
4  similar to what one would get from calling memory_dff with -nordff.

```

**C.109 memory\_share – consolidate memory ports**

```

1  memory_share [selection]
2
3  This pass merges share-able memory ports into single memory ports.
4
5  The following methods are used to consolidate the number of memory ports:
6
7  - When write ports are connected to async read ports accessing the same
8    address, then this feedback path is converted to a write port with
9    byte/part enable signals.
10
11 - When multiple write ports access the same address then this is converted
12   to a single write port with a more complex data and/or enable logic path.
13
14 - When multiple write ports are never accessed at the same time (a SAT
15   solver is used to determine this), then the ports are merged into a single
16   write port.
17
18 Note that in addition to the algorithms implemented in this pass, the $memrd
19 and $memwr cells are also subject to generic resource sharing passes (and other
20 optimizations) such as "share" and "opt_merge".

```

**C.110 memory\_unpack – unpack multi-port memory cells**

```

1  memory_unpack [selection]
2
3  This pass converts the multi-port $mem memory cells into individual $memrd and
4  $memwr cells. It is the counterpart to the memory_collect pass.

```

**C.111 miter – automatically create a miter circuit**

```

1  miter -equiv [options] gold_name gate_name miter_name
2
3  Creates a miter circuit for equivalence checking. The gold- and gate- modules
4  must have the same interfaces. The miter circuit will have all inputs of the
5  two source modules, prefixed with 'in_'. The miter circuit has a 'trigger'
6  output that goes high if an output mismatch between the two source modules is
7  detected.
8
9  -ignore_gold_x
10     a undef (x) bit in the gold module output will match any value in
11     the gate module output.
12
13  -make_outputs
14     also route the gold- and gate-outputs to 'gold_*' and 'gate_*' outputs
15     on the miter circuit.
16
17  -make_outcmp

```

```

18         also create a cmp_* output for each gold/gate output pair.
19
20     -make_assert
21         also create an 'assert' cell that checks if trigger is always low.
22
23     -flatten
24         call 'flatten -wb; opt_expr -keepdc -undriven;;' on the miter circuit.
25
26
27     miter -assert [options] module [miter_name]
28
29     Creates a miter circuit for property checking. All input ports are kept,
30     output ports are discarded. An additional output 'trigger' is created that
31     goes high when an assert is violated. Without a miter_name, the existing
32     module is modified.
33
34     -make_outputs
35         keep module output ports.
36
37     -flatten
38         call 'flatten -wb; opt_expr -keepdc -undriven;;' on the miter circuit.

```

### C.112 mutate – generate or apply design mutations

```

1     mutate -list N [options] [selection]
2
3     Create a list of N mutations using an even sampling.
4
5     -o filename
6         Write list to this file instead of console output
7
8     -s filename
9         Write a list of all src tags found in the design to the specified file
10
11     -seed N
12         RNG seed for selecting mutations
13
14     -none
15         Include a "none" mutation in the output
16
17     -ctrl name width value
18         Add -ctrl options to the output. Use 'value' for first mutation, then
19         simply count up from there.
20
21     -mode name
22     -module name
23     -cell name
24     -port name
25     -portbit int
26     -ctrlbit int
27     -wire name
28     -wirebit int

```

```

29  -src string
30      Filter list of mutation candidates to those matching
31      the given parameters.
32
33  -cfg option int
34      Set a configuration option. Options available:
35      weight_pq_w weight_pq_b weight_pq_c weight_pq_s
36      weight_pq_mw weight_pq_mb weight_pq_mc weight_pq_ms
37      weight_cover pick_cover_prnt
38
39
40  mutate -mode MODE [options]
41
42  Apply the given mutation.
43
44  -ctrl name width value
45      Add a control signal with the given name and width. The mutation is
46      activated if the control signal equals the given value.
47
48  -module name
49  -cell name
50  -port name
51  -portbit int
52  -ctrlbit int
53      Mutation parameters, as generated by 'mutate -list N'.
54
55  -wire name
56  -wirebit int
57  -src string
58      Ignored. (They are generated by -list for documentation purposes.)

```

### C.113 muxcover – cover trees of MUX cells with wider MUXes

```

1  muxcover [options] [selection]
2
3  Cover trees of $_MUX_ cells with $_MUX{4,8,16}_ cells
4
5  -mux4[=cost], -mux8[=cost], -mux16[=cost]
6      Cover $_MUX_ trees using the specified types of MUXes (with optional
7      integer costs). If none of these options are given, the effect is the
8      same as if all of them are.
9      Default costs: $_MUX4_ = 220, $_MUX8_ = 460,
10                     $_MUX16_ = 940
11
12  -mux2=cost
13      Use the specified cost for $_MUX_ cells when making covering decisions.
14      Default cost: $_MUX_ = 100
15
16  -dmux=cost
17      Use the specified cost for $_MUX_ cells used in decoders.
18      Default cost: 90
19

```

```

20  -nodecode
21      Do not insert decoder logic. This reduces the number of possible
22      substitutions, but guarantees that the resulting circuit is not
23      less efficient than the original circuit.
24
25  -nopartial
26      Do not consider mappings that use $_MUX<N>_ to select from less
27      than <N> different signals.

```

### C.114 muxpack – \$mux/\$pmux cascades to \$pmux

```

1  muxpack [selection]
2
3  This pass converts cascaded chains of $pmux cells (e.g. those create from case
4  constructs) and $mux cells (e.g. those created by if-else constructs) into
5  $pmux cells.
6
7  This optimisation is conservative --- it will only pack $mux or $pmux cells
8  whose select lines are driven by '$eq' cells with other such cells if it can be
9  certain that their select inputs are mutually exclusive.

```

### C.115 nlutmap – map to LUTs of different sizes

```

1  nlutmap [options] [selection]
2
3  This pass uses successive calls to 'abc' to map to an architecture. That
4  provides a small number of differently sized LUTs.
5
6  -luts N_1,N_2,N_3,...
7      The number of LUTs with 1, 2, 3, ... inputs that are
8      available in the target architecture.
9
10 -assert
11     Create an error if not all logic can be mapped
12
13 Excess logic that does not fit into the specified LUTs is mapped back
14 to generic logic gates ($_AND_, etc.).

```

### C.116 onehot – optimize \$eq cells for onehot signals

```

1  onehot [options] [selection]
2
3  This pass optimizes $eq cells that compare one-hot signals against constants
4
5  -v, -vv
6      verbose output

```



**C.117 opt – perform simple optimizations**

```

1      opt [options] [selection]
2
3  This pass calls all the other opt_* passes in a useful order. This performs
4  a series of trivial optimizations and cleanups. This pass executes the other
5  passes in the following order:
6
7      opt_expr [-mux_undef] [-mux_bool] [-undriven] [-clkinv] [-fine] [-full] [-keepdc]
8      opt_merge [-share_all] -nomux
9
10     do
11         opt_muxtree
12         opt_reduce [-fine] [-full]
13         opt_merge [-share_all]
14         opt_share (-full only)
15         opt_rmdff [-keepdc] [-sat]
16         opt_clean [-purge]
17         opt_expr [-mux_undef] [-mux_bool] [-undriven] [-clkinv] [-fine] [-full] [-keepdc]
18     while <changed design>
19
20  When called with -fast the following script is used instead:
21
22     do
23         opt_expr [-mux_undef] [-mux_bool] [-undriven] [-clkinv] [-fine] [-full] [-keepdc]
24         opt_merge [-share_all]
25         opt_rmdff [-keepdc] [-sat]
26         opt_clean [-purge]
27     while <changed design in opt_rmdff>
28
29  Note: Options in square brackets (such as [-keepdc]) are passed through to
30  the opt_* commands when given to 'opt'.

```

**C.118 opt\_clean – remove unused cells and wires**

```

1      opt_clean [options] [selection]
2
3  This pass identifies wires and cells that are unused and removes them. Other
4  passes often remove cells but leave the wires in the design or reconnect the
5  wires but leave the old cells in the design. This pass can be used to clean up
6  after the passes that do the actual work.
7
8  This pass only operates on completely selected modules without processes.
9
10     -purge
11         also remove internal nets if they have a public name

```

**C.119 opt\_demorgan – Optimize reductions with DeMorgan equivalents**

```

1  opt_demorgan [selection]
2
3  This pass pushes inverters through $reduce_* cells if this will reduce the
4  overall gate count of the circuit

```

## C.120 opt\_expr – perform const folding and simple expression rewriting

```

1  opt_expr [options] [selection]
2
3  This pass performs const folding on internal cell types with constant inputs.
4  It also performs some simple expression rewriting.
5
6  -mux_undef
7      remove 'undef' inputs from $mux, $pmux and $_MUX_ cells
8
9  -mux_bool
10     replace $mux cells with inverters or buffers when possible
11
12  -undriven
13     replace undriven nets with undef (x) constants
14
15  -clkinv
16     optimize clock inverters by changing FF types
17
18  -fine
19     perform fine-grain optimizations
20
21  -full
22     alias for -mux_undef -mux_bool -undriven -fine
23
24  -keepdc
25     some optimizations change the behavior of the circuit with respect to
26     don't-care bits. for example in 'a+0' a single x-bit in 'a' will cause
27     all result bits to be set to x. this behavior changes when 'a+0' is
28     replaced by 'a'. the -keepdc option disables all such optimizations.

```

## C.121 opt\_lut – optimize LUT cells

```

1  opt_lut [options] [selection]
2
3  This pass combines cascaded $lut cells with unused inputs.
4
5  -dlogic <type>:<cell-port>=<LUT-input>[:<cell-port>=<LUT-input>...]
6      preserve connections to dedicated logic cell <type> that has ports
7      <cell-port> connected to LUT inputs <LUT-input>. this includes
8      the case where both LUT and dedicated logic input are connected to
9      the same constant.

```

```

10
11     -limit N
12         only perform the first N combines, then stop. useful for debugging.

```

### C.122 **opt\_lut\_ins** – discard unused LUT inputs

```

1     opt_lut_ins [options] [selection]
2
3     This pass removes unused inputs from LUT cells (that is, inputs that can not
4     influence the output signal given this LUT's value). While such LUTs cannot
5     be directly emitted by ABC, they can be a result of various post-ABC
6     transformations, such as mapping wide LUTs (not all sub-LUTs will use the
7     full set of inputs) or optimizations such as xilinx_dffopt.
8
9     -tech <technology>
10         Instead of generic $lut cells, operate on LUT cells specific
11         to the given technology. Valid values are: xilinx, ecp5, gowin.

```

### C.123 **opt\_mem** – optimize memories

```

1     opt_mem [options] [selection]
2
3     This pass performs various optimizations on memories in the design.

```

### C.124 **opt\_merge** – consolidate identical cells

```

1     opt_merge [options] [selection]
2
3     This pass identifies cells with identical type and input signals. Such cells
4     are then merged to one cell.
5
6     -nomux
7         Do not merge MUX cells.
8
9     -share_all
10        Operate on all cell types, not just built-in types.

```

### C.125 **opt\_muxtree** – eliminate dead trees in multiplexer trees

```

1     opt_muxtree [selection]
2
3     This pass analyzes the control signals for the multiplexer trees in the design
4     and identifies inputs that can never be active. It then removes this dead
5     branches from the multiplexer trees.
6
7     This pass only operates on completely selected modules without processes.

```

**C.126 opt\_reduce – simplify large MUXes and AND/OR gates**

```

1  opt_reduce [options] [selection]
2
3  This pass performs two interlinked optimizations:
4
5  1. it consolidates trees of large AND gates or OR gates and eliminates
6  duplicated inputs.
7
8  2. it identifies duplicated inputs to MUXes and replaces them with a single
9  input with the original control signals OR'ed together.
10
11  -fine
12      perform fine-grain optimizations
13
14  -full
15      alias for -fine

```

**C.127 opt\_rmdff – remove DFFs with constant inputs**

```

1  opt_rmdff [-keepdc] [-sat] [selection]
2
3  This pass identifies flip-flops with constant inputs and replaces them with
4  a constant driver.
5
6  -sat
7      additionally invoke SAT solver to detect and remove flip-flops (with
8      non-constant inputs) that can also be replaced with a constant driver

```

**C.128 opt\_share – merge mutually exclusive cells of the same type that share an input signal**

```

1  opt_share [selection]
2
3  This pass identifies mutually exclusive cells of the same type that:
4  (a) share an input signal,
5  (b) drive the same $mux, $_MUX_, or $pmux multiplexing cell,
6
7  allowing the cell to be merged and the multiplexer to be moved from
8  multiplexing its output to multiplexing the non-shared input signals.

```

**C.129 paramap – renaming cell parameters**

```

1  paramap [options] [selection]
2
3  This command renames cell parameters and/or maps key/value pairs to

```

```

4 other key/value pairs.
5
6 -tocase <name>
7     Match attribute names case-insensitively and set it to the specified
8     name.
9
10 -rename <old_name> <new_name>
11     Rename attributes as specified
12
13 -map <old_name>=<old_value> <new_name>=<new_value>
14     Map key/value pairs as indicated.
15
16 -imap <old_name>=<old_value> <new_name>=<new_value>
17     Like -map, but use case-insensitive match for <old_value> when
18     it is a string value.
19
20 -remove <name>=<value>
21     Remove attributes matching this pattern.
22
23 For example, mapping Diamond-style ECP5 "init" attributes to Yosys-style:
24
25 paramap -tocase INIT t:LUT4

```

### C.130 peepopt – collection of peephole optimizers

```

1     peepopt [options] [selection]
2
3 This pass applies a collection of peephole optimizers to the current design.

```

### C.131 plugin – load and list loaded plugins

```

1     plugin [options]
2
3 Load and list loaded plugins.
4
5 -i <plugin_filename>
6     Load (install) the specified plugin.
7
8 -a <alias_name>
9     Register the specified alias name for the loaded plugin
10
11 -l
12     List loaded plugins

```

### C.132 pmux2shiftx – transform \$pmux cells to \$shiftx cells

```

1  pmux2shiftx [options] [selection]
2
3  This pass transforms $pmux cells to $shiftx cells.
4
5  -v, -vv
6      verbose output
7
8  -min_density <percentage>
9      specifies the minimum density for the shifter
10     default: 50
11
12  -min_choices <int>
13     specified the minimum number of choices for a control signal
14     default: 3
15
16  -onehot ignore|pmux|shiftx
17     select strategy for one-hot encoded control signals
18     default: pmux
19
20  -norange
21     disable $sub inference for "range decoders"

```

### C.133 pmuxtree – transform \$pmux cells to trees of \$mux cells

```

1  pmuxtree [selection]
2
3  This pass transforms $pmux cells to trees of $mux cells.

```

### C.134 portlist – list (top-level) ports

```

1  portlist [options] [selection]
2
3  This command lists all module ports found in the selected modules.
4
5  If no selection is provided then it lists the ports on the top module.
6
7  -m
8      print verilog blackbox module definitions instead of port lists

```

### C.135 prep – generic synthesis script

```

1  prep [options]
2
3  This command runs a conservative RTL synthesis. A typical application for this
4  is the preparation stage of a verification flow. This command does not operate
5  on partly selected designs.

```

```

6
7  -top <module>
8      use the specified module as top module (default='top')
9
10 -auto-top
11     automatically determine the top of the design hierarchy
12
13 -flatten
14     flatten the design before synthesis. this will pass '-auto-top' to
15     'hierarchy' if no top module is specified.
16
17 -ifx
18     passed to 'proc'. uses verilog simulation behavior for verilog if/case
19     undef handling. this also prevents 'wreduce' from being run.
20
21 -memx
22     simulate verilog simulation behavior for out-of-bounds memory accesses
23     using the 'memory_memx' pass.
24
25 -nomem
26     do not run any of the memory_* passes
27
28 -rdff
29     do not pass -nordff to 'memory_dff'. This enables merging of FFs into
30     memory read ports.
31
32 -nokeepdc
33     do not call opt_* with -keepdc
34
35 -run <from_label>[:<to_label>]
36     only run the commands between the labels (see below). an empty
37     from label is synonymous to 'begin', and empty to label is
38     synonymous to the end of the command list.
39
40
41 The following commands are executed by this synthesis command:
42
43 begin:
44     hierarchy -check [-top <top> | -auto-top]
45
46 coarse:
47     proc [-ifx]
48     flatten    (if -flatten)
49     opt_expr -keepdc
50     opt_clean
51     check
52     opt -keepdc
53     wreduce -keepdc [-memx]
54     memory_dff [-nordff]
55     memory_memx    (if -memx)
56     opt_clean
57     memory_collect
58     opt -keepdc -fast
59

```

```

60     check:
61         stat
62         check

```

### C.136 `proc` – translate processes to netlists

```

1     proc [options] [selection]
2
3 This pass calls all the other proc_* passes in the most common order.
4
5     proc_clean
6     proc_rmdead
7     proc_prune
8     proc_init
9     proc_arst
10    proc_mux
11    proc_dlatch
12    proc_dff
13    proc_clean
14
15 This replaces the processes in the design with multiplexers,
16 flip-flops and latches.
17
18 The following options are supported:
19
20     -global_arst [!]<netname>
21         This option is passed through to proc_arst.
22
23     -ifx
24         This option is passed through to proc_mux. proc_rmdead is not
25         executed in -ifx mode.

```

### C.137 `proc_arst` – detect asynchronous resets

```

1     proc_arst [-global_arst [!]<netname>] [selection]
2
3 This pass identifies asynchronous resets in the processes and converts them
4 to a different internal representation that is suitable for generating
5 flip-flop cells with asynchronous resets.
6
7     -global_arst [!]<netname>
8         In modules that have a net with the given name, use this net as async
9         reset for registers that have been assign initial values in their
10        declaration ('reg foobar = constant_value;'). Use the '!' modifier for
11        active low reset signals. Note: the frontend stores the default value
12        in the 'init' attribute on the net.

```



**C.138 proc\_clean – remove empty parts of processes**

```

1  proc_clean [options] [selection]
2
3  -quiet
4      do not print any messages.
5
6  This pass removes empty parts of processes and ultimately removes a process
7  if it contains only empty structures.
```

**C.139 proc\_dff – extract flip-flops from processes**

```

1  proc_dff [selection]
2
3  This pass identifies flip-flops in the processes and converts them to
4  d-type flip-flop cells.
```

**C.140 proc\_dlatch – extract latches from processes**

```

1  proc_dlatch [selection]
2
3  This pass identifies latches in the processes and converts them to
4  d-type latches.
```

**C.141 proc\_init – convert initial block to init attributes**

```

1  proc_init [selection]
2
3  This pass extracts the 'init' actions from processes (generated from Verilog
4  'initial' blocks) and sets the initial value to the 'init' attribute on the
5  respective wire.
```

**C.142 proc\_mux – convert decision trees to multiplexers**

```

1  proc_mux [options] [selection]
2
3  This pass converts the decision trees in processes (originating from if-else
4  and case statements) to trees of multiplexer cells.
5
6  -ifx
7      Use Verilog simulation behavior with respect to undef values in
8      'case' expressions and 'if' conditions.
```

**C.143 proc\_prune – remove redundant assignments**

```

1  proc_prune [selection]
2
3  This pass identifies assignments in processes that are always overwritten by
4  a later assignment to the same signal and removes them.

```

**C.144 proc\_rmdead – eliminate dead trees in decision trees**

```

1  proc_rmdead [selection]
2
3  This pass identifies unreachable branches in decision trees and removes them.

```

**C.145 qwp – quadratic wirelength placer**

```

1  qwp [options] [selection]
2
3  This command runs quadratic wirelength placement on the selected modules and
4  annotates the cells in the design with 'qwp_position' attributes.
5
6  -ltr
7      Add left-to-right constraints: constrain all inputs on the left border
8      outputs to the right border.
9
10 -alpha
11     Add constraints for inputs/outputs to be placed in alphanumerical
12     order along the y-axis (top-to-bottom).
13
14 -grid N
15     Number of grid divisions in x- and y-direction. (default=16)
16
17 -dump <html_file_name>
18     Dump a protocol of the placement algorithm to the html file.
19
20 -v
21     Verbose solver output for profiling or debugging
22
23 Note: This implementation of a quadratic wirelength placer uses exact
24 dense matrix operations. It is only a toy-placer for small circuits.

```

**C.146 read – load HDL designs**

```

1  read {-vlog95|-vlog2k|-sv2005|-sv2009|-sv2012|-sv|-formal} <verilog-file>..
2
3  Load the specified Verilog/SystemVerilog files. (Full SystemVerilog support
4  is only available via Verific.)
5

```

```

6 Additional -D<macro>[=<value>] options may be added after the option indicating
7 the language version (and before file names) to set additional verilog defines.
8
9
10 read {-vhd187|-vhd193|-vhd12k|-vhd12008|-vhd1} <vhd1-file>..
11
12 Load the specified VHDL files. (Requires Verific.)
13
14
15 read -define <macro>[=<value>]..
16
17 Set global Verilog/SystemVerilog defines.
18
19
20 read -undef <macro>..
21
22 Unset global Verilog/SystemVerilog defines.
23
24
25 read -incdir <directory>
26
27 Add directory to global Verilog/SystemVerilog include directories.
28
29
30 read -verific
31 read -noverific
32
33 Subsequent calls to 'read' will either use or not use Verific. Calling 'read'
34 with -verific will result in an error on Yosys binaries that are built without
35 Verific support. The default is to use Verific if it is available.

```

### C.147 read\_aiger – read AIGER file

```

1 read_aiger [options] [filename]
2
3 Load module from an AIGER file into the current design.
4
5 -module_name <module_name>
6     name of module to be created (default: <filename>)
7
8 -clk_name <wire_name>
9     if specified, AIGER latches to be transformed into $_DFF_P_ cells
10    clocked by wire of this name. otherwise, $_FF_ cells will be used
11
12 -map <filename>
13     read file with port and latch symbols
14
15 -wideports
16     merge ports that match the pattern 'name[int]' into a single
17     multi-bit port 'name'
18
19 -xaiger

```

20 | read XAIGER extensions

### C.148 read\_blif – read BLIF file

```

1   read_blif [options] [filename]
2
3   Load modules from a BLIF file into the current design.
4
5   -sop
6       Create $sop cells instead of $lut cells
7
8   -wideports
9       Merge ports that match the pattern 'name[int]' into a single
10      multi-bit port 'name'.
```

### C.149 read\_ilang – read modules from ilang file

```

1   read_ilang [filename]
2
3   Load modules from an ilang file to the current design. (ilang is a text
4   representation of a design in yosys's internal format.)
5
6   -nooverwrite
7       ignore re-definitions of modules. (the default behavior is to
8       create an error message if the existing module is not a blackbox
9       module, and overwrite the existing module if it is a blackbox module.)
10
11  -overwrite
12      overwrite existing modules with the same name
13
14  -lib
15      only create empty blackbox modules
```

### C.150 read\_json – read JSON file

```

1   read_json [filename]
2
3   Load modules from a JSON file into the current design See "help write_json"
4   for a description of the file format.
```

### C.151 read\_liberty – read cells from liberty file

```

1  read_liberty [filename]
2
3  Read cells from liberty file as modules into current design.
4
5  -lib
6      only create empty blackbox modules
7
8  -nooverwrite
9      ignore re-definitions of modules. (the default behavior is to
10     create an error message if the existing module is not a blackbox
11     module, and overwrite the existing module if it is a blackbox module.)
12
13  -overwrite
14     overwrite existing modules with the same name
15
16  -ignore_miss_func
17     ignore cells with missing function specification of outputs
18
19  -ignore_miss_dir
20     ignore cells with a missing or invalid direction
21     specification on a pin
22
23  -ignore_miss_data_latch
24     ignore latches with missing data and/or enable pins
25
26  -setattr <attribute_name>
27     set the specified attribute (to the value 1) on all loaded modules

```

### C.152 read\_verilog – read modules from Verilog file

```

1  read_verilog [options] [filename]
2
3  Load modules from a Verilog file to the current design. A large subset of
4  Verilog-2005 is supported.
5
6  -sv
7      enable support for SystemVerilog features. (only a small subset
8      of SystemVerilog is supported)
9
10  -formal
11     enable support for SystemVerilog assertions and some Yosys extensions
12     replace the implicit -D SYNTHESIS with -D FORMAL
13
14  -noassert
15     ignore assert() statements
16
17  -noassume
18     ignore assume() statements
19
20  -norestrict
21     ignore restrict() statements

```

```

22
23 -assume-asserts
24     treat all assert() statements like assume() statements
25
26 -assert-assumes
27     treat all assume() statements like assert() statements
28
29 -debug
30     alias for -dump_ast1 -dump_ast2 -dump_vlog1 -dump_vlog2 -yydebug
31
32 -dump_ast1
33     dump abstract syntax tree (before simplification)
34
35 -dump_ast2
36     dump abstract syntax tree (after simplification)
37
38 -no_dump_ptr
39     do not include hex memory addresses in dump (easier to diff dumps)
40
41 -dump_vlog1
42     dump ast as Verilog code (before simplification)
43
44 -dump_vlog2
45     dump ast as Verilog code (after simplification)
46
47 -dump_rtlil
48     dump generated RTLIL netlist
49
50 -yydebug
51     enable parser debug output
52
53 -nolatches
54     usually latches are synthesized into logic loops
55     this option prohibits this and sets the output to 'x'
56     in what would be the latches hold condition
57
58     this behavior can also be achieved by setting the
59     'nolatches' attribute on the respective module or
60     always block.
61
62 -nomem2reg
63     under certain conditions memories are converted to registers
64     early during simplification to ensure correct handling of
65     complex corner cases. this option disables this behavior.
66
67     this can also be achieved by setting the 'nomem2reg'
68     attribute on the respective module or register.
69
70     This is potentially dangerous. Usually the front-end has good
71     reasons for converting an array to a list of registers.
72     Prohibiting this step will likely result in incorrect synthesis
73     results.
74
75 -mem2reg

```

```

76         always convert memories to registers. this can also be
77         achieved by setting the 'mem2reg' attribute on the respective
78         module or register.
79
80     -nomeminit
81         do not infer $meminit cells and instead convert initialized
82         memories to registers directly in the front-end.
83
84     -ppdump
85         dump Verilog code after pre-processor
86
87     -nopp
88         do not run the pre-processor
89
90     -nodpi
91         disable DPI-C support
92
93     -noblackbox
94         do not automatically add a (* blackbox *) attribute to an
95         empty module.
96
97     -lib
98         only create empty blackbox modules. This implies -DBLACKBOX.
99         modules with the (* whitebox *) attribute will be preserved.
100        (* lib_whitebox *) will be treated like (* whitebox *).
101
102     -nowb
103         delete (* whitebox *) and (* lib_whitebox *) attributes from
104         all modules.
105
106     -specify
107         parse and import specify blocks
108
109     -noopt
110         don't perform basic optimizations (such as const folding) in the
111         high-level front-end.
112
113     -icells
114         interpret cell types starting with '$' as internal cell types
115
116     -pwires
117         add a wire for each module parameter
118
119     -nooverwrite
120         ignore re-definitions of modules. (the default behavior is to
121         create an error message if the existing module is not a black box
122         module, and overwrite the existing module otherwise.)
123
124     -overwrite
125         overwrite existing modules with the same name
126
127     -defer
128         only read the abstract syntax tree and defer actual compilation
129         to a later 'hierarchy' command. Useful in cases where the default

```

```

130     parameters of modules yield invalid or not synthesizable code.
131
132     -noautowire
133         make the default of 'default_nettype be "none" instead of "wire".
134
135     -setattr <attribute_name>
136         set the specified attribute (to the value 1) on all loaded modules
137
138     -Dname[=definition]
139         define the preprocessor symbol 'name' and set its optional value
140         'definition'
141
142     -Idir
143         add 'dir' to the directories which are used when searching include
144         files
145
146 The command 'verilog_defaults' can be used to register default options for
147 subsequent calls to 'read_verilog'.
148
149 Note that the Verilog frontend does a pretty good job of processing valid
150 verilog input, but has not very good error reporting. It generally is
151 recommended to use a simulator (for example Icarus Verilog) for checking
152 the syntax of the code, rather than to rely on read_verilog for that.
153
154 Depending on if read_verilog is run in -formal mode, either the macro
155 SYNTHESIS or FORMAL is defined automatically. In addition, read_verilog
156 always defines the macro YOSYS.
157
158 See the Yosys README file for a list of non-standard Verilog features
159 supported by the Yosys Verilog front-end.

```

### C.153 rename – rename object in the design

```

1     rename old_name new_name
2
3 Rename the specified object. Note that selection patterns are not supported
4 by this command.
5
6
7
8     rename -output old_name new_name
9
10 Like above, but also make the wire an output. This will fail if the object is
11 not a wire.
12
13
14     rename -src [selection]
15
16 Assign names auto-generated from the src attribute to all selected wires and
17 cells with private names.
18
19

```



```

20     rename -wire [selection]
21
22 Assign auto-generated names based on the wires they drive to all selected
23 cells with private names. Ignores cells driving privately named wires.
24
25
26     rename -enumerate [-pattern <pattern>] [selection]
27
28 Assign short auto-generated names to all selected wires and cells with private
29 names. The -pattern option can be used to set the pattern for the new names.
30 The character % in the pattern is replaced with a integer number. The default
31 pattern is '_%_'.
32
33
34     rename -hide [selection]
35
36 Assign private names (the ones with $-prefix) to all selected wires and cells
37 with public names. This ignores all selected ports.
38
39
40     rename -top new_name
41
42 Rename top module.

```

### C.154 rmports – remove module ports with no connections

```

1     rmports [selection]
2
3 This pass identifies ports in the selected modules which are not used or
4 driven and removes them.

```

### C.155 sat – solve a SAT problem in the circuit

```

1     sat [options] [selection]
2
3 This command solves a SAT problem defined over the currently selected circuit
4 and additional constraints passed as parameters.
5
6     -all
7         show all solutions to the problem (this can grow exponentially, use
8         -max <N> instead to get <N> solutions)
9
10    -max <N>
11        like -all, but limit number of solutions to <N>
12
13    -enable_undef
14        enable modeling of undef value (aka 'x-bits')
15        this option is implied by -set-def, -set-undef et. cetera
16
17    -max_undef

```

```

18         maximize the number of undef bits in solutions, giving a better
19         picture of which input bits are actually vital to the solution.
20
21     -set <signal> <value>
22         set the specified signal to the specified value.
23
24     -set-def <signal>
25         add a constraint that all bits of the given signal must be defined
26
27     -set-any-undef <signal>
28         add a constraint that at least one bit of the given signal is undefined
29
30     -set-all-undef <signal>
31         add a constraint that all bits of the given signal are undefined
32
33     -set-def-inputs
34         add -set-def constraints for all module inputs
35
36     -show <signal>
37         show the model for the specified signal. if no -show option is
38         passed then a set of signals to be shown is automatically selected.
39
40     -show-inputs, -show-outputs, -show-ports
41         add all module (input/output) ports to the list of shown signals
42
43     -show-regs, -show-public, -show-all
44         show all registers, show signals with 'public' names, show all signals
45
46     -ignore_div_by_zero
47         ignore all solutions that involve a division by zero
48
49     -ignore_unknown_cells
50         ignore all cells that can not be matched to a SAT model
51
52 The following options can be used to set up a sequential problem:
53
54     -seq <N>
55         set up a sequential problem with <N> time steps. The steps will
56         be numbered from 1 to N.
57
58         note: for large <N> it can be significantly faster to use
59         -tempinduct-baseonly -maxsteps <N> instead of -seq <N>.
60
61     -set-at <N> <signal> <value>
62     -unset-at <N> <signal>
63         set or unset the specified signal to the specified value in the
64         given timestep. this has priority over a -set for the same signal.
65
66     -set-assumes
67         set all assumptions provided via $assume cells
68
69     -set-def-at <N> <signal>
70     -set-any-undef-at <N> <signal>
71     -set-all-undef-at <N> <signal>

```

```

72         add undef constraints in the given timestep.
73
74     -set-init <signal> <value>
75         set the initial value for the register driving the signal to the value
76
77     -set-init-undef
78         set all initial states (not set using -set-init) to undef
79
80     -set-init-def
81         do not force a value for the initial state but do not allow undef
82
83     -set-init-zero
84         set all initial states (not set using -set-init) to zero
85
86     -dump_vcd <vcd-file-name>
87         dump SAT model (counter example in proof) to VCD file
88
89     -dump_json <json-file-name>
90         dump SAT model (counter example in proof) to a WaveJSON file.
91
92     -dump_cnf <cnf-file-name>
93         dump CNF of SAT problem (in DIMACS format). in temporal induction
94         proofs this is the CNF of the first induction step.
95
96 The following additional options can be used to set up a proof. If also -seq
97 is passed, a temporal induction proof is performed.
98
99     -tempinduct
100         Perform a temporal induction proof. In a temporal induction proof it is
101         proven that the condition holds forever after the number of time steps
102         specified using -seq.
103
104     -tempinduct-def
105         Perform a temporal induction proof. Assume an initial state with all
106         registers set to defined values for the induction step.
107
108     -tempinduct-baseonly
109         Run only the basecase half of temporal induction (requires -maxsteps)
110
111     -tempinduct-inductonly
112         Run only the induction half of temporal induction
113
114     -tempinduct-skip <N>
115         Skip the first <N> steps of the induction proof.
116
117         note: this will assume that the base case holds for <N> steps.
118         this must be proven independently with "-tempinduct-baseonly
119         -maxsteps <N>". Use -initsteps if you just want to set a
120         minimal induction length.
121
122     -prove <signal> <value>
123         Attempt to proof that <signal> is always <value>.
124
125     -prove-x <signal> <value>

```

```

126     Like -prove, but an undef (x) bit in the lhs matches any value on
127     the right hand side. Useful for equivalence checking.
128
129     -prove-asserts
130         Prove that all asserts in the design hold.
131
132     -prove-skip <N>
133         Do not enforce the prove-condition for the first <N> time steps.
134
135     -maxsteps <N>
136         Set a maximum length for the induction.
137
138     -initsteps <N>
139         Set initial length for the induction.
140         This will speed up the search of the right induction length
141         for deep induction proofs.
142
143     -stepsize <N>
144         Increase the size of the induction proof in steps of <N>.
145         This will speed up the search of the right induction length
146         for deep induction proofs.
147
148     -timeout <N>
149         Maximum number of seconds a single SAT instance may take.
150
151     -verify
152         Return an error and stop the synthesis script if the proof fails.
153
154     -verify-no-timeout
155         Like -verify but do not return an error for timeouts.
156
157     -falsify
158         Return an error and stop the synthesis script if the proof succeeds.
159
160     -falsify-no-timeout
161         Like -falsify but do not return an error for timeouts.

```

### C.156 scatter – add additional intermediate nets

```

1     scatter [selection]
2
3     This command adds additional intermediate nets on all cell ports. This is used
4     for testing the correct use of the SigMap helper in passes. If you don't know
5     what this means: don't worry -- you only need this pass when testing your own
6     extensions to Yosys.
7
8     Use the opt_clean command to get rid of the additional nets.

```

### C.157 scc – detect strongly connected components (logic loops)

```

1  scc [options] [selection]
2
3  This command identifies strongly connected components (aka logic loops) in the
4  design.
5
6  -expect <num>
7      expect to find exactly <num> SSCs. A different number of SSCs will
8      produce an error.
9
10 -max_depth <num>
11     limit to loops not longer than the specified number of cells. This
12     can e.g. be useful in identifying small local loops in a module that
13     implements one large SCC.
14
15 -nofeedback
16     do not count cells that have their output fed back into one of their
17     inputs as single-cell scc.
18
19 -all_cell_types
20     Usually this command only considers internal non-memory cells. With
21     this option set, all cells are considered. For unknown cells all ports
22     are assumed to be bidirectional 'inout' ports.
23
24 -set_attr <name> <value>
25     set the specified attribute on all cells that are part of a logic
26     loop. the special token {} in the value is replaced with a unique
27     identifier for the logic loop.
28
29 -select
30     replace the current selection with a selection of all cells and wires
31     that are part of a found logic loop

```

### C.158 scratchpad – get/set values in the scratchpad

```

1  scratchpad [options]
2
3  This pass allows to read and modify values from the scratchpad of the current
4  design. Options:
5
6  -get <identifier>
7      print the value saved in the scratchpad under the given identifier.
8
9  -set <identifier> <value>
10     save the given value in the scratchpad under the given identifier.
11
12 -unset <identifier>
13     remove the entry for the given identifier from the scratchpad.
14
15 -copy <identifier_from> <identifier_to>
16     copy the value of the first identifier to the second identifier.
17

```

```

18  -assert <identifier> <value>
19      assert that the entry for the given identifier is set to the given value.
20
21  -assert-set <identifier>
22      assert that the entry for the given identifier exists.
23
24  -assert-unset <identifier>
25      assert that the entry for the given identifier does not exist.
26
27  The identifier may not contain whitespace. By convention, it is usually prefixed
28  by the name of the pass that uses it, e.g. 'opt.did_something'. If the value
29  contains whitespace, it must be enclosed in double quotes.

```

### C.159 script – execute commands from file or wire

```

1  script <filename> [<from_label>:<to_label>]
2  script -scriptwire [selection]
3
4  This command executes the yosys commands in the specified file (default
5  behaviour), or commands embedded in the constant text value connected to the
6  selected wires.
7
8  In the default (file) case, the 2nd argument can be used to only execute the
9  section of the file between the specified labels. An empty from label is
10 synonymous with the beginning of the file and an empty to label is synonymous
11 with the end of the file.
12
13 If only one label is specified (without ':') then only the block
14 marked with that label (until the next label) is executed.
15
16 In "-scriptwire" mode, the commands on the selected wire(s) will be executed
17 in the scope of (and thus, relative to) the wires' owning module(s). This
18 '-module' mode can be exited by using the 'cd' command.

```

### C.160 select – modify and view the list of selected objects

```

1  select [ -add | -del | -set <name> ] {-read <filename> | <selection>}
2  select [ <assert_option> ] {-read <filename> | <selection>}
3  select [ -list | -write <filename> | -count | -clear ]
4  select -module <modname>
5
6  Most commands use the list of currently selected objects to determine which part
7  of the design to operate on. This command can be used to modify and view this
8  list of selected objects.
9
10 Note that many commands support an optional [selection] argument that can be
11 used to override the global selection for the command. The syntax of this
12 optional argument is identical to the syntax of the <selection> argument
13 described here.
14

```

```

15  -add, -del
16      add or remove the given objects to the current selection.
17      without this options the current selection is replaced.
18
19  -set <name>
20      do not modify the current selection. instead save the new selection
21      under the given name (see @<name> below). to save the current selection,
22      use "select -set <name> %"
23
24  -assert-none
25      do not modify the current selection. instead assert that the given
26      selection is empty. i.e. produce an error if any object matching the
27      selection is found.
28
29  -assert-any
30      do not modify the current selection. instead assert that the given
31      selection is non-empty. i.e. produce an error if no object matching
32      the selection is found.
33
34  -assert-count N
35      do not modify the current selection. instead assert that the given
36      selection contains exactly N objects.
37
38  -assert-max N
39      do not modify the current selection. instead assert that the given
40      selection contains less than or exactly N objects.
41
42  -assert-min N
43      do not modify the current selection. instead assert that the given
44      selection contains at least N objects.
45
46  -list
47      list all objects in the current selection
48
49  -write <filename>
50      like -list but write the output to the specified file
51
52  -read <filename>
53      read the specified file (written by -write)
54
55  -count
56      count all objects in the current selection
57
58  -clear
59      clear the current selection. this effectively selects the whole
60      design. it also resets the selected module (see -module). use the
61      command 'select *' to select everything but stay in the current module.
62
63  -none
64      create an empty selection. the current module is unchanged.
65
66  -module <modname>
67      limit the current scope to the specified module.
68      the difference between this and simply selecting the module

```

is that all object names are interpreted relative to this module after this command until the selection is cleared again.

When this command is called without an argument, the current selection is displayed in a compact form (i.e. only the module name when a whole module is selected).

The <selection> argument itself is a series of commands for a simple stack machine. Each element on the stack represents a set of selected objects. After this commands have been executed, the union of all remaining sets on the stack is computed and used as selection for the command.

Pushing (selecting) object when not in -module mode:

```
<mod_pattern>
    select the specified module(s)
```

```
<mod_pattern>/<obj_pattern>
    select the specified object(s) from the module(s)
```

Pushing (selecting) object when in -module mode:

```
<obj_pattern>
    select the specified object(s) from the current module
```

A <mod\_pattern> can be a module name, wildcard expression (\*, ?, [...]) matching module names, or one of the following:

```
A:<pattern>, A:<pattern>=<pattern>
    all modules with an attribute matching the given pattern
    in addition to = also <, <=, >=, and > are supported
```

```
N:<pattern>
    all modules with a name matching the given pattern
    (i.e. 'N:' is optional as it is the default matching rule)
```

An <obj\_pattern> can be an object name, wildcard expression, or one of the following:

```
w:<pattern>
    all wires with a name matching the given wildcard pattern
```

```
i:<pattern>, o:<pattern>, x:<pattern>
    all inputs (i:), outputs (o:) or any ports (x:) with matching names
```

```
s:<size>, s:<min>:<max>
    all wires with a matching width
```

```
m:<pattern>
    all memories with a name matching the given pattern
```

```
c:<pattern>
    all cells with a name matching the given pattern
```



```

123 t:<pattern>
124     all cells with a type matching the given pattern
125
126 p:<pattern>
127     all processes with a name matching the given pattern
128
129 a:<pattern>
130     all objects with an attribute name matching the given pattern
131
132 a:<pattern>=<pattern>
133     all objects with a matching attribute name-value-pair.
134     in addition to = also <, <=, >=, and > are supported
135
136 r:<pattern>, r:<pattern>=<pattern>
137     cells with matching parameters. also with <, <=, >= and >.
138
139 n:<pattern>
140     all objects with a name matching the given pattern
141     (i.e. 'n:' is optional as it is the default matching rule)
142
143 @<name>
144     push the selection saved prior with 'select -set <name> ...'
145

```

The following actions can be performed on the top sets on the stack:

```

147
148 %
149     push a copy of the current selection to the stack
150
151 %%
152     replace the stack with a union of all elements on it
153
154 %n
155     replace top set with its invert
156
157 %u
158     replace the two top sets on the stack with their union
159
160 %i
161     replace the two top sets on the stack with their intersection
162
163 %d
164     pop the top set from the stack and subtract it from the new top
165
166 %D
167     like %d but swap the roles of two top sets on the stack
168
169 %c
170     create a copy of the top set from the stack and push it
171
172 %x[<num1>|*][.<num2>][:<rule>[:<rule>..]]
173     expand top set <num1> num times according to the specified rules.
174     (i.e. select all cells connected to selected wires and select all
175     wires connected to selected cells) The rules specify which cell
176     ports to use for this. the syntax for a rule is a '-' for exclusion

```

```

177 and a '+' for inclusion, followed by an optional comma separated
178 list of cell types followed by an optional comma separated list of
179 cell ports in square brackets. a rule can also be just a cell or wire
180 name that limits the expansion (is included but does not go beyond).
181 select at most <num2> objects. a warning message is printed when this
182 limit is reached. When '*' is used instead of <num1> then the process
183 is repeated until no further object are selected.
184
185 %ci[<num1>|*][.<num2>][:<rule>[:<rule>..]]
186 %co[<num1>|*][.<num2>][:<rule>[:<rule>..]]
187     similar to %x, but only select input (%ci) or output cones (%co)
188
189 %xe[...] %cie[...] %coe
190     like %x, %ci, and %co but only consider combinatorial cells
191
192 %a
193     expand top set by selecting all wires that are (at least in part)
194     aliases for selected wires.
195
196 %s
197     expand top set by adding all modules that implement cells in selected
198     modules
199
200 %m
201     expand top set by selecting all modules that contain selected objects
202
203 %M
204     select modules that implement selected cells
205
206 %C
207     select cells that implement selected modules
208
209 %R[<num>]
210     select <num> random objects from top selection (default 1)
211
212 Example: the following command selects all wires that are connected to a
213 'GATE' input of a 'SWITCH' cell:
214
215 select */t:SWITCH %x:+[GATE] */t:SWITCH %d

```

### C.161 setattr – set/unset attributes on objects

```

1   setattr [ -mod ] [ -set name value | -unset name ]... [selection]
2
3   Set/unset the given attributes on the selected objects. String values must be
4   passed in double quotes (").
5
6   When called with -mod, this command will set and unset attributes on modules
7   instead of objects within modules.

```

**C.162 setparam – set/unset parameters on objects**

```

1   setparam [ -type cell_type ] [ -set name value | -unset name ]... [selection]
2
3   Set/unset the given parameters on the selected cells. String values must be
4   passed in double quotes (").
5
6   The -type option can be used to change the cell type of the selected cells.
```

**C.163 setundef – replace undef values with defined constants**

```

1   setundef [options] [selection]
2
3   This command replaces undef (x) constants with defined (0/1) constants.
4
5   -undriven
6       also set undriven nets to constant values
7
8   -expose
9       also expose undriven nets as inputs (use with -undriven)
10
11  -zero
12      replace with bits cleared (0)
13
14  -one
15      replace with bits set (1)
16
17  -undef
18      replace with undef (x) bits, may be used with -undriven
19
20  -anyseq
21      replace with $anyseq drivers (for formal)
22
23  -anyconst
24      replace with $anyconst drivers (for formal)
25
26  -random <seed>
27      replace with random bits using the specified integer as seed
28      value for the random number generator.
29
30  -init
31      also create/update init values for flip-flops
32
33  -params
34      replace undef in cell parameters
```

**C.164 sf2\_iobs – SF2: insert IO buffers**

```

1      sf2_iobs [options] [selection]
2
3  Add SF2 I/O buffers and global buffers to top module as needed.
4
5      -clkbuf
6          Insert PAD->global_net clock buffers

```

## C.165 share – perform sat-based resource sharing

```

1      share [options] [selection]
2
3  This pass merges shareable resources into a single resource. A SAT solver
4  is used to determine if two resources are share-able.
5
6      -force
7          Per default the selection of cells that is considered for sharing is
8          narrowed using a list of cell types. With this option all selected
9          cells are considered for resource sharing.
10
11          IMPORTANT NOTE: If the -all option is used then no cells with internal
12          state must be selected!
13
14      -aggressive
15          Per default some heuristics are used to reduce the number of cells
16          considered for resource sharing to only large resources. This options
17          turns this heuristics off, resulting in much more cells being considered
18          for resource sharing.
19
20      -fast
21          Only consider the simple part of the control logic in SAT solving, resulting
22          in much easier SAT problems at the cost of maybe missing some opportunities
23          for resource sharing.
24
25      -limit N
26          Only perform the first N merges, then stop. This is useful for debugging.

```

## C.166 shell – enter interactive command mode

```

1      shell
2
3  This command enters the interactive command mode. This can be useful
4  in a script to interrupt the script at a certain point and allow for
5  interactive inspection or manual synthesis of the design at this point.
6
7  The command prompt of the interactive shell indicates the current
8  selection (see 'help select'):
9
10      yosys>
11          the entire design is selected

```

```

12
13 yosys*>
14     only part of the design is selected
15
16 yosys [modname]>
17     the entire module 'modname' is selected using 'select -module modname'
18
19 yosys [modname]*>
20     only part of current module 'modname' is selected
21
22 When in interactive shell, some errors (e.g. invalid command arguments)
23 do not terminate yosys but return to the command prompt.
24
25 This command is the default action if nothing else has been specified
26 on the command line.
27
28 Press Ctrl-D or type 'exit' to leave the interactive shell.

```

## C.167 show – generate schematics using graphviz

```

1 show [options] [selection]
2
3 Create a graphviz DOT file for the selected part of the design and compile it
4 to a graphics file (usually SVG or PostScript).
5
6 -viewer <viewer>
7     Run the specified command with the graphics file as parameter.
8     On Windows, this pauses yosys until the viewer exits.
9
10 -format <format>
11     Generate a graphics file in the specified format. Use 'dot' to just
12     generate a .dot file, or other <format> strings such as 'svg' or 'ps'
13     to generate files in other formats (this calls the 'dot' command).
14
15 -lib <verilog_or_ilang_file>
16     Use the specified library file for determining whether cell ports are
17     inputs or outputs. This option can be used multiple times to specify
18     more than one library.
19
20     note: in most cases it is better to load the library before calling
21     show with 'read_verilog -lib <filename>'. it is also possible to
22     load liberty files with 'read_liberty -lib <filename>'.
23
24 -prefix <prefix>
25     generate <prefix>.* instead of ~/.yosys_show.*
26
27 -color <color> <object>
28     assign the specified color to the specified object. The object can be
29     a single selection wildcard expressions or a saved set of objects in
30     the @<name> syntax (see "help select" for details).
31
32 -label <text> <object>

```

```

33         assign the specified label text to the specified object. The object can
34         be a single selection wildcard expressions or a saved set of objects in
35         the @<name> syntax (see "help select" for details).
36
37     -colors <seed>
38         Randomly assign colors to the wires. The integer argument is the seed
39         for the random number generator. Change the seed value if the colored
40         graph still is ambiguous. A seed of zero deactivates the coloring.
41
42     -colorattr <attribute_name>
43         Use the specified attribute to assign colors. A unique color is
44         assigned to each unique value of this attribute.
45
46     -width
47         annotate buses with a label indicating the width of the bus.
48
49     -signed
50         mark ports (A, B) that are declared as signed (using the [AB]_SIGNED
51         cell parameter) with an asterisk next to the port name.
52
53     -stretch
54         stretch the graph so all inputs are on the left side and all outputs
55         (including inout ports) are on the right side.
56
57     -pause
58         wait for the use to press enter to before returning
59
60     -enum
61         enumerate objects with internal ($-prefixed) names
62
63     -long
64         do not abbreviate objects with internal ($-prefixed) names
65
66     -notitle
67         do not add the module name as graph title to the dot file
68
69     -nobg
70         don't run viewer in the background, IE wait for the viewer tool to
71         exit before returning
72
73     When no <format> is specified, 'dot' is used. When no <format> and <viewer> is
74     specified, 'xdot' is used to display the schematic (POSIX systems only).
75
76     The generated output files are '~/yosys_show.dot' and '~/yosys_show.<format>',
77     unless another prefix is specified using -prefix <prefix>.
78
79     Yosys on Windows and YosysJS use different defaults: The output is written
80     to 'show.dot' in the current directory and new viewer is launched each time
81     the 'show' command is executed.

```

## C.168 shregmap – map shift registers

```

1  shregmap [options] [selection]
2
3  This pass converts chains of $_DFF_[NP]_ gates to target specific shift register
4  primitives. The generated shift register will be of type $__SHREG_DFF_[NP]_ and
5  will use the same interface as the original $_DFF_*_ cells. The cell parameter
6  'DEPTH' will contain the depth of the shift register. Use a target-specific
7  'techmap' map file to convert those cells to the actual target cells.
8
9  -minlen N
10     minimum length of shift register (default = 2)
11     (this is the length after -keep_before and -keep_after)
12
13  -maxlen N
14     maximum length of shift register (default = no limit)
15     larger chains will be mapped to multiple shift register instances
16
17  -keep_before N
18     number of DFFs to keep before the shift register (default = 0)
19
20  -keep_after N
21     number of DFFs to keep after the shift register (default = 0)
22
23  -clkpol pos|neg|any
24     limit match to only positive or negative edge clocks. (default = any)
25
26  -enpol pos|neg|none|any_or_none|any
27     limit match to FFs with the specified enable polarity. (default = none)
28
29  -match <cell_type>[:<d_port_name>:<q_port_name>]
30     match the specified cells instead of $_DFF_N_ and $_DFF_P_. If
31     '[:<d_port_name>:<q_port_name>]' is omitted then 'D' and 'Q' is used
32     by default. E.g. the option '-clkpol pos' is just an alias for
33     '-match $_DFF_P_', which is an alias for '-match $_DFF_P_:D:Q'.
34
35  -params
36     instead of encoding the clock and enable polarity in the cell name by
37     deriving from the original cell name, simply name all generated cells
38     $__SHREG_ and use CLKPOL and ENPOL parameters. An ENPOL value of 2 is
39     used to denote cells without enable input. The ENPOL parameter is
40     omitted when '-enpol none' (or no -enpol option) is passed.
41
42  -zinit
43     assume the shift register is automatically zero-initialized, so it
44     becomes legal to merge zero initialized FFs into the shift register.
45
46  -init
47     map initialized registers to the shift reg, add an INIT parameter to
48     generated cells with the initialization value. (first bit to shift out
49     in LSB position)
50
51  -tech greenpak4
52     map to greenpak4 shift registers.

```

**C.169 sim – simulate the circuit**

```

1  sim [options] [top-level]
2
3  This command simulates the circuit using the given top-level module.
4
5  -vcd <filename>
6      write the simulation results to the given VCD file
7
8  -clock <portname>
9      name of top-level clock input
10
11 -clockn <portname>
12     name of top-level clock input (inverse polarity)
13
14 -reset <portname>
15     name of top-level reset input (active high)
16
17 -resetn <portname>
18     name of top-level inverted reset input (active low)
19
20 -rstlen <integer>
21     number of cycles reset should stay active (default: 1)
22
23 -zinit
24     zero-initialize all uninitialized regs and memories
25
26 -n <integer>
27     number of cycles to simulate (default: 20)
28
29 -a
30     include all nets in VCD output, not just those with public names
31
32 -w
33     writeback mode: use final simulation state as new init state
34
35 -d
36     enable debug output

```

**C.170 simplemap – mapping simple coarse-grain cells**

```

1  simplemap [selection]
2
3  This pass maps a small selection of simple coarse-grain cells to yosys gate
4  primitives. The following internal cell types are mapped by this pass:
5
6  $not, $pos, $and, $or, $xor, $xnor
7  $reduce_and, $reduce_or, $reduce_xor, $reduce_xnor, $reduce_bool
8  $logic_not, $logic_and, $logic_or, $mux, $tribuf
9  $sr, $ff, $dff, $dffsr, $adff, $dlatch

```



**C.171 splice – create explicit splicing cells**

```

1 splice [options] [selection]
2
3 This command adds $slice and $concat cells to the design to make the splicing
4 of multi-bit signals explicit. This for example is useful for coarse grain
5 synthesis, where dedicated hardware is needed to splice signals.
6
7 -sel_by_cell
8     only select the cell ports to rewire by the cell. if the selection
9     contains a cell, than all cell inputs are rewired, if necessary.
10
11 -sel_by_wire
12     only select the cell ports to rewire by the wire. if the selection
13     contains a wire, than all cell ports driven by this wire are wired,
14     if necessary.
15
16 -sel_any_bit
17     it is sufficient if the driver of any bit of a cell port is selected.
18     by default all bits must be selected.
19
20 -wires
21     also add $slice and $concat cells to drive otherwise unused wires.
22
23 -no_outputs
24     do not rewire selected module outputs.
25
26 -port <name>
27     only rewire cell ports with the specified name. can be used multiple
28     times. implies -no_output.
29
30 -no_port <name>
31     do not rewire cell ports with the specified name. can be used multiple
32     times. can not be combined with -port <name>.
33
34 By default selected output wires and all cell ports of selected cells driven
35 by selected wires are rewired.

```

**C.172 splitnets – split up multi-bit nets**

```

1 splitnets [options] [selection]
2
3 This command splits multi-bit nets into single-bit nets.
4
5 -format char1[char2[char3]]
6     the first char is inserted between the net name and the bit index, the
7     second char is appended to the netname. e.g. -format () creates net
8     names like 'mysignal(42)'. the 3rd character is the range separation
9     character when creating multi-bit wires. the default is '[]:'.
10
11 -ports
12     also split module ports. per default only internal signals are split.

```

```

13 |
14 | -driver
15 |     don't blindly split nets in individual bits. instead look at the driver
16 |     and split nets so that no driver drives only part of a net.

```

### C.173 stat – print some statistics

```

1 |     stat [options] [selection]
2 |
3 | Print some statistics (number of objects) on the selected portion of the
4 | design.
5 |
6 | -top <module>
7 |     print design hierarchy with this module as top. if the design is fully
8 |     selected and a module has the 'top' attribute set, this module is used
9 |     default value for this option.
10 |
11 | -liberty <liberty_file>
12 |     use cell area information from the provided liberty file
13 |
14 | -tech <technology>
15 |     print area estimate for the specified technology. Currently supported
16 |     values for <technology>: xilinx, cmos
17 |
18 | -width
19 |     annotate internal cell types with their word width.
20 |     e.g. $add_8 for an 8 bit wide $add cell.

```

### C.174 submod – moving part of a module to a new submodule

```

1 |     submod [options] [selection]
2 |
3 | This pass identifies all cells with the 'submod' attribute and moves them to
4 | a newly created module. The value of the attribute is used as name for the
5 | cell that replaces the group of cells with the same attribute value.
6 |
7 | This pass can be used to create a design hierarchy in flat design. This can
8 | be useful for analyzing or reverse-engineering a design.
9 |
10 | This pass only operates on completely selected modules with no processes
11 | or memories.
12 |
13 | -copy
14 |     by default the cells are 'moved' from the source module and the source
15 |     module will use an instance of the new module after this command is
16 |     finished. call with -copy to not modify the source module.
17 |
18 | -name <name>
19 |     don't use the 'submod' attribute but instead use the selection. only
20 |     objects from one module might be selected. the value of the -name option

```

```

21         is used as the value of the 'submod' attribute instead.
22
23     -hidden
24         instead of creating submodule ports with public names, create ports with
25         private names so that a subsequent 'flatten; clean' call will restore the
26         original module with original public names.

```

### C.175 supercover – add hi/lo cover cells for each wire bit

```

1     supercover [options] [selection]
2
3     This command adds two cover cells for each bit of each selected wire, one
4     checking for a hi signal level and one checking for lo level.

```

### C.176 synth – generic synthesis script

```

1     synth [options]
2
3     This command runs the default synthesis script. This command does not operate
4     on partly selected designs.
5
6     -top <module>
7         use the specified module as top module (default='top')
8
9     -auto-top
10        automatically determine the top of the design hierarchy
11
12     -flatten
13        flatten the design before synthesis. this will pass '-auto-top' to
14        'hierarchy' if no top module is specified.
15
16     -encfile <file>
17        passed to 'fsm_recode' via 'fsm'
18
19     -lut <k>
20        perform synthesis for a k-LUT architecture.
21
22     -nofsm
23        do not run FSM optimization
24
25     -noabc
26        do not run abc (as if yosys was compiled without ABC support)
27
28     -noalumacc
29        do not run 'alumacc' pass. i.e. keep arithmetic operators in
30        their direct form ($add, $sub, etc.).
31
32     -nordff
33        passed to 'memory'. prohibits merging of FFs into memory read ports
34

```

```

35 -noshare
36     do not run SAT-based resource sharing
37
38 -run <from_label>[:<to_label>]
39     only run the commands between the labels (see below). an empty
40     from label is synonymous to 'begin', and empty to label is
41     synonymous to the end of the command list.
42
43 -abc9
44     use new ABC9 flow (EXPERIMENTAL)
45
46 -flowmap
47     use FlowMap LUT techmapping instead of ABC
48
49
50 The following commands are executed by this synthesis command:
51
52 begin:
53     hierarchy -check [-top <top> | -auto-top]
54
55 coarse:
56     proc
57     flatten      (if -flatten)
58     opt_expr
59     opt_clean
60     check
61     opt
62     wreduce
63     peepopt
64     opt_clean
65     techmap -map +/cmp2lut.v -map +/cmp2lcu.v      (if -lut)
66     alumacc      (unless -noalumacc)
67     share        (unless -noshare)
68     opt
69     fsm          (unless -nofsm)
70     opt -fast
71     memory -nomap
72     opt_clean
73
74 fine:
75     opt -fast -full
76     memory_map
77     opt -full
78     techmap
79     techmap -map +/gate2lut.v      (if -noabc and -lut)
80     clean; opt_lut                (if -noabc and -lut)
81     flowmap -maxlut K              (if -flowmap and -lut)
82     opt -fast
83     abc -fast                      (unless -noabc, unless -lut)
84     abc -fast -lut k               (unless -noabc, if -lut)
85     opt -fast                      (unless -noabc)
86
87 check:
88     hierarchy -check

```

```

89     stat
90     check

```

## C.177 synth\_achronix – synthesis for Achronix Speedster22i FPGAs.

```

1     synth_achronix [options]
2
3     This command runs synthesis for Achronix Speedster eFPGAs. This work is still experime
4
5     -top <module>
6         use the specified module as top module (default='top')
7
8     -vout <file>
9         write the design to the specified Verilog netlist file. writing of an
10        output file is omitted if this parameter is not specified.
11
12     -run <from_label>:<to_label>
13         only run the commands between the labels (see below). an empty
14         from label is synonymous to 'begin', and empty to label is
15         synonymous to the end of the command list.
16
17     -noflatten
18         do not flatten design before synthesis
19
20     -retime
21         run 'abc' with '-dff -D 1' options
22
23
24     The following commands are executed by this synthesis command:
25
26     begin:
27         read_verilog -sv -lib +/achronix/speedster22i/cells_sim.v
28         hierarchy -check -top <top>
29
30     flatten:      (unless -noflatten)
31         proc
32         flatten
33         tribuf -logic
34         deminout
35
36     coarse:
37         synth -run coarse
38
39     fine:
40         opt -fast -mux_undef -undriven -fine -full
41         memory_map
42         opt -undriven -fine
43         dff2dfffe -direct-match $_DFF_*
44         opt -fine
45         techmap -map +/techmap.v
46         opt -full
47         clean -purge

```

```

48     setundef -undriven -zero
49     abc -markgroups -dff -D 1      (only if -retime)
50
51 map_luts:
52     abc -lut 4
53     clean
54
55 map_cells:
56     iopadmap -bits -outpad $__outpad I:O -inpad $__inpad O:I
57     techmap -map +/achronix/speedster22i/cells_map.v
58     clean -purge
59
60 check:
61     hierarchy -check
62     stat
63     check -noinit
64
65 vout:
66     write_verilog -nodec -attr2comment -defparam -renameprefix syn_ <file-name>

```

## C.178 synth\_anlogic – synthesis for Anlogic FPGAs

```

1     synth_anlogic [options]
2
3 This command runs synthesis for Anlogic FPGAs.
4
5 -top <module>
6     use the specified module as top module
7
8 -edif <file>
9     write the design to the specified EDIF file. writing of an output file
10    is omitted if this parameter is not specified.
11
12 -json <file>
13    write the design to the specified JSON file. writing of an output file
14    is omitted if this parameter is not specified.
15
16 -run <from_label>:<to_label>
17    only run the commands between the labels (see below). an empty
18    from label is synonymous to 'begin', and empty to label is
19    synonymous to the end of the command list.
20
21 -noflatten
22    do not flatten design before synthesis
23
24 -retime
25    run 'abc' with '-dff -D 1' options
26
27 -nolutram
28    do not use EG_LOGIC_DRAM16X4 cells in output netlist
29
30

```

```

31 The following commands are executed by this synthesis command:
32
33 begin:
34     read_verilog -lib +/anlogic/cells_sim.v +/anlogic/eagle_bb.v
35     hierarchy -check -top <top>
36
37 flatten:      (unless -noflatten)
38     proc
39     flatten
40     tribuf -logic
41     deminout
42
43 coarse:
44     synth -run coarse
45
46 map_lutram:    (skip if -nolutram)
47     memory_bram -rules +/anlogic/lutrams.txt
48     techmap -map +/anlogic/lutrams_map.v
49     setundef -zero -params t:EG_LOGIC_DRAM16X4
50
51 map_ffram:
52     opt -fast -mux_undef -undriven -fine
53     memory_map
54     opt -undriven -fine
55
56 map_gates:
57     techmap -map +/techmap.v -map +/anlogic/arith_map.v
58     opt -fast
59     abc -dff -D 1      (only if -retime)
60
61 map_ffs:
62     techmap -D NO_LUT -map +/anlogic/cells_map.v
63     dffinit -strinit SET RESET -ff AL_MAP_SEQ q REGSET -noreinit
64     opt_expr -mux_undef
65     simplemap
66
67 map_luts:
68     abc -lut 4:6
69     clean
70
71 map_cells:
72     techmap -map +/anlogic/cells_map.v
73     clean
74
75 map_anlogic:
76     anlogic_fixcarry
77     anlogic_eqn
78
79 check:
80     hierarchy -check
81     stat
82     check -noinit
83
84 edif:

```

```

85     write_edif <file-name>
86
87     json:
88         write_json <file-name>

```

### C.179 synth\_coolrunner2 – synthesis for Xilinx Coolrunner-II CPLDs

```

1     synth_coolrunner2 [options]
2
3     This command runs synthesis for Coolrunner-II CPLDs. This work is experimental.
4     It is intended to be used with https://github.com/azonenberg/openfpga as the
5     place-and-route.
6
7     -top <module>
8         use the specified module as top module (default='top')
9
10    -json <file>
11        write the design to the specified JSON file. writing of an output file
12        is omitted if this parameter is not specified.
13
14    -run <from_label>:<to_label>
15        only run the commands between the labels (see below). an empty
16        from label is synonymous to 'begin', and empty to label is
17        synonymous to the end of the command list.
18
19    -noflatten
20        do not flatten design before synthesis
21
22    -retime
23        run 'abc' with '-dff -D 1' options
24
25
26    The following commands are executed by this synthesis command:
27
28    begin:
29        read_verilog -lib +/coolrunner2/cells_sim.v
30        hierarchy -check -top <top>
31
32    flatten:      (unless -noflatten)
33        proc
34        flatten
35        tribuf -logic
36
37    coarse:
38        synth -run coarse
39
40    fine:
41        extract_counter -dir up -allow_arst no
42        techmap -map +/coolrunner2/cells_counter_map.v
43        clean
44        opt -fast -full
45        techmap -map +/techmap.v -map +/coolrunner2/cells_latch.v

```



```

46     opt -fast
47     dfflibmap -prepare -liberty +/coolrunner2/xc2_dff.lib
48
49 map_tff:
50     abc -g AND,XOR
51     clean
52     extract -map +/coolrunner2/tff_extract.v
53
54 map_pla:
55     abc -sop -I 40 -P 56
56     clean
57
58 map_cells:
59     dfflibmap -liberty +/coolrunner2/xc2_dff.lib
60     dffinit -ff FDCP Q INIT
61     dffinit -ff FDCP_N Q INIT
62     dffinit -ff FTCP Q INIT
63     dffinit -ff FTCP_N Q INIT
64     dffinit -ff LDCP Q INIT
65     dffinit -ff LDCP_N Q INIT
66     coolrunner2_sop
67     clean
68     iopadmap -bits -inpad IBUF O:I -outpad IOBUFE I:IO -inoutpad IOBUFE O:IO -tout
69     attrmvp -attr src -attr LOC t:IOBUFE n:*
70     attrmvp -attr src -attr LOC -driven t:IBUF n:*
71     coolrunner2_fixup
72     splitnets
73     clean
74
75 check:
76     hierarchy -check
77     stat
78     check -noinit
79
80 json:
81     write_json <file-name>

```

## C.180 synth\_easic – synthesis for eASIC platform

```

1     synth_easic [options]
2
3 This command runs synthesis for eASIC platform.
4
5     -top <module>
6         use the specified module as top module
7
8     -vlog <file>
9         write the design to the specified structural Verilog file. writing of
10        an output file is omitted if this parameter is not specified.
11
12     -etools <path>
13        set path to the eTools installation. (default=/opt/eTools)

```

```

14
15 -run <from_label>:<to_label>
16     only run the commands between the labels (see below). an empty
17     from label is synonymous to 'begin', and empty to label is
18     synonymous to the end of the command list.
19
20 -noflatten
21     do not flatten design before synthesis
22
23 -retime
24     run 'abc' with '-dff -D 1' options
25
26

```

The following commands are executed by this synthesis command:

```

28
29 begin:
30     read_liberty -lib <etools_phys_clk_lib>
31     read_liberty -lib <etools_logic_lut_lib>
32     hierarchy -check -top <top>
33
34 flatten:      (unless -noflatten)
35     proc
36     flatten
37
38 coarse:
39     synth -run coarse
40
41 fine:
42     opt -fast -mux_undef -undriven -fine
43     memory_map
44     opt -undriven -fine
45     techmap
46     opt -fast
47     abc -dff -D 1      (only if -retime)
48     opt_clean      (only if -retime)
49
50 map:
51     dfflibmap -liberty <etools_phys_clk_lib>
52     abc -liberty <etools_logic_lut_lib>
53     opt_clean
54
55 check:
56     hierarchy -check
57     stat
58     check -noinit
59
60 vlog:
61     write_verilog -noexpr -attr2comment <file-name>

```

## C.181 synth\_ecp5 – synthesis for ECP5 FPGAs

```

1 synth_ecp5 [options]

```

This command runs synthesis for ECP5 FPGAs.

```

-top <module>
    use the specified module as top module

-blif <file>
    write the design to the specified BLIF file. writing of an output file
    is omitted if this parameter is not specified.

-edif <file>
    write the design to the specified EDIF file. writing of an output file
    is omitted if this parameter is not specified.

-json <file>
    write the design to the specified JSON file. writing of an output file
    is omitted if this parameter is not specified.

-run <from_label>:<to_label>
    only run the commands between the labels (see below). an empty
    from label is synonymous to 'begin', and empty to label is
    synonymous to the end of the command list.

-noflatten
    do not flatten design before synthesis

-retime
    run 'abc' with '-dff -D 1' options

-noccu2
    do not use CCU2 cells in output netlist

-nodffe
    do not use flipflops with CE in output netlist

-nobram
    do not use block RAM cells in output netlist

-nolutram
    do not use LUT RAM cells in output netlist

-nowidelut
    do not use PFU muxes to implement LUTs larger than LUT4s

-asyncprld
    use async PRLD mode to implement DLATCH and DFFSR (EXPERIMENTAL)

-abc2
    run two passes of 'abc' for slightly improved logic density

-abc9
    use new ABC9 flow (EXPERIMENTAL)

-vpr

```

56 generate an output netlist (and BLIF file) suitable for VPR  
 57 (this feature is experimental and incomplete)

58  
 59 -nodsp  
 60 do not map multipliers to MULT18X18D

61  
 62  
 63 The following commands are executed by this synthesis command:

64  
 65 begin:  
 66 read\_verilog -lib -specify +/ecp5/cells\_sim.v +/ecp5/cells\_bb.v  
 67 hierarchy -check -top <top>

68  
 69 coarse:  
 70 proc  
 71 flatten  
 72 tribuf -logic  
 73 deminout  
 74 opt\_expr  
 75 opt\_clean  
 76 check  
 77 opt  
 78 wreduce  
 79 peepopt  
 80 opt\_clean  
 81 share  
 82 techmap -map +/cmp2lut.v -D LUT\_WIDTH=4  
 83 opt\_expr  
 84 opt\_clean  
 85 techmap -map +/mul2dsp.v -map +/ecp5/dsp\_map.v -D DSP\_A\_MAXWIDTH=18 -D DSP\_B\_M  
 -D DSP\_A\_MINWIDTH=2 -D DSP\_B\_MINWIDTH=2 -D DSP\_NAME=\_\_MUL18X18 (unless -nodsp)  
 86 ctype -set \$mul t:\$\_\_soft\_mul (unless -nodsp)  
 87 alumacc  
 88 opt  
 89 fsm  
 90 opt -fast  
 91 memory -nomap  
 92 opt\_clean

93  
 94 map\_bram: (skip if -nobram)  
 95 memory\_bram -rules +/ecp5/brams.txt  
 96 techmap -map +/ecp5/brams\_map.v

97  
 98 map\_lutram: (skip if -nolutram)  
 99 memory\_bram -rules +/ecp5/lutrams.txt  
 100 techmap -map +/ecp5/lutrams\_map.v

101  
 102 map\_ffram:  
 103 opt -fast -mux\_undef -undriven -fine  
 104 memory\_map -iattr -attr !ram\_block -attr !rom\_block -attr logic\_block -attr sy  
 105 opt -undriven -fine

106  
 107 map\_gates:  
 108 techmap -map +/techmap.v -map +/ecp5/arith\_map.v

```

109     opt -fast
110     abc -dff -D 1      (only if -retime)
111
112 map_ffs:
113     dff2dffs
114     opt_clean
115     dff2dfffe -direct-match $_DFF_* -direct-match $__DFFS_*
116     techmap -D NO_LUT [-D ASYNC_PRLD] -map +/ecp5/cells_map.v
117     opt_expr -undriven -mux_undef
118     simplemap
119     ecp5_ffinit
120     ecp5_gsr
121     attrmvp -copy -attr syn_useioff
122     opt_clean
123
124 map_luts:
125     abc              (only if -abc2)
126     techmap -map +/ecp5/latches_map.v
127     abc -lut 4:7 -dress
128     clean
129
130 map_cells:
131     techmap -map +/ecp5/cells_map.v      (with -D NO_LUT in vpr mode)
132     opt_lut_ins -tech ecp5
133     clean
134
135 check:
136     autoname
137     hierarchy -check
138     stat
139     check -noinit
140
141 blif:
142     opt_clean -purge                                (vpr mode)
143     write_blif -attr -cname -conn -param <file-name> (vpr mode)
144     write_blif -gates -attr -param <file-name>      (non-vpr mode)
145
146 edif:
147     write_edif <file-name>
148
149 json:
150     write_json <file-name>

```

## C.182 synth\_efinix – synthesis for Efinix FPGAs

```

1 synth_efinix [options]
2
3 This command runs synthesis for Efinix FPGAs.
4
5 -top <module>
6     use the specified module as top module
7

```

```

8  -edif <file>
9      write the design to the specified EDIF file. writing of an output file
10     is omitted if this parameter is not specified.
11
12  -json <file>
13      write the design to the specified JSON file. writing of an output file
14     is omitted if this parameter is not specified.
15
16  -run <from_label>:<to_label>
17      only run the commands between the labels (see below). an empty
18     from label is synonymous to 'begin', and empty to label is
19     synonymous to the end of the command list.
20
21  -noflatten
22      do not flatten design before synthesis
23
24  -retime
25      run 'abc' with '-dff -D 1' options
26
27  -nobram
28      do not use EFX_RAM_5K cells in output netlist
29
30
31  The following commands are executed by this synthesis command:
32
33  begin:
34      read_verilog -lib +/efinix/cells_sim.v
35      hierarchy -check -top <top>
36
37  flatten:      (unless -noflatten)
38      proc
39      flatten
40      tribuf -logic
41      deminout
42
43  coarse:
44      synth -run coarse
45      memory_bram -rules +/efinix/brams.txt
46      techmap -map +/efinix/brams_map.v
47      setundef -zero -params t:EFX_RAM_5K
48
49  map_ffram:
50      opt -fast -mux_undef -undriven -fine
51      memory_map
52      opt -undriven -fine
53
54  map_gates:
55      techmap -map +/techmap.v -map +/efinix/arith_map.v
56      opt -fast
57      abc -dff -D 1      (only if -retime)
58
59  map_ffs:
60      techmap -D NO_LUT -map +/efinix/cells_map.v
61      dffinit -strinit SET RESET -ff AL_MAP_SEQ q REGSET -noreinit

```

```

62     opt_expr -mux_undef
63     simplemap
64
65 map_luts:
66     abc -lut 4
67     clean
68
69 map_cells:
70     techmap -map +/efinix/cells_map.v
71     clean
72
73 map_gbuf:
74     efinix_gbuf
75     efinix_fixcarry
76     clean
77
78 check:
79     hierarchy -check
80     stat
81     check -noinit
82
83 edif:
84     write_edif <file-name>
85
86 json:
87     write_json <file-name>

```

### C.183 synth\_gowin – synthesis for Gowin FPGAs

```

1     synth_gowin [options]
2
3 This command runs synthesis for Gowin FPGAs. This work is experimental.
4
5 -top <module>
6     use the specified module as top module (default='top')
7
8 -vout <file>
9     write the design to the specified Verilog netlist file. writing of an
10    output file is omitted if this parameter is not specified.
11
12 -run <from_label>:<to_label>
13    only run the commands between the labels (see below). an empty
14    from label is synonymous to 'begin', and empty to label is
15    synonymous to the end of the command list.
16
17 -nodffe
18    do not use flipflops with CE in output netlist
19
20 -nobram
21    do not use BRAM cells in output netlist
22
23 -nolutram

```

```

24         do not use distributed RAM cells in output netlist
25
26     -noflatten
27         do not flatten design before synthesis
28
29     -retime
30         run 'abc' with '-dff -D 1' options
31
32     -nowidelut
33         do not use muxes to implement LUTs larger than LUT4s
34
35     -noiopads
36         do not emit IOB at top level ports
37
38
39 The following commands are executed by this synthesis command:
40
41     begin:
42         read_verilog -lib +/gowin/cells_sim.v
43         hierarchy -check -top <top>
44
45     flatten:      (unless -noflatten)
46         proc
47         flatten
48         tribuf -logic
49         deminout
50
51     coarse:
52         synth -run coarse
53
54     map_bram:      (skip if -nobram)
55         memory_bram -rules +/gowin/brams.txt
56         techmap -map +/gowin/brams_map.v
57
58     map_lutram:    (skip if -nolutram)
59         memory_bram -rules +/gowin/lutrams.txt
60         techmap -map +/gowin/lutrams_map.v
61         determine_init
62
63     map_ffram:
64         opt -fast -mux_undef -undriven -fine
65         memory_map
66         opt -undriven -fine
67
68     map_gates:
69         techmap -map +/techmap.v -map +/gowin/arith_map.v
70         opt -fast
71         abc -dff -D 1      (only if -retime)
72         splitnets
73
74     map_ffs:
75         dff2dffs -match-init
76         opt_clean
77         dff2dfte -direct-match $_DFF_* -direct-match $__DFFS_*

```



```

78     techmap -map +/gowin/cells_map.v
79     opt_expr -mux_undef
80     simplemap
81
82     map_luts:
83         abc -lut 4:8
84         clean
85
86     map_cells:
87         techmap -map +/gowin/cells_map.v
88         opt_lut_ins -tech gowin
89         setundef -undriven -params -zero
90         hilomap -singleton -hicell VCC V -locell GND G
91         iopadmap -bits -inpad IBUF O:I -outpad OBUF I:O -toutpad TBUF OEN:I:O -tinoutp
(unless -noiopads)
92         clean
93
94     check:
95         hierarchy -check
96         stat
97         check -noinit
98
99     vout:
100     write_verilog -decimal -attr2comment -defparam -renameprefix gen <file-name>

```

## C.184 synth\_greenpak4 – synthesis for GreenPAK4 FPGAs

```

1     synth_greenpak4 [options]
2
3     This command runs synthesis for GreenPAK4 FPGAs. This work is experimental.
4     It is intended to be used with https://github.com/azonenberg/openfpga as the
5     place-and-route.
6
7     -top <module>
8         use the specified module as top module (default='top')
9
10    -part <part>
11        synthesize for the specified part. Valid values are SLG46140V,
12        SLG46620V, and SLG46621V (default).
13
14    -json <file>
15        write the design to the specified JSON file. writing of an output file
16        is omitted if this parameter is not specified.
17
18    -run <from_label>:<to_label>
19        only run the commands between the labels (see below). an empty
20        from label is synonymous to 'begin', and empty to label is
21        synonymous to the end of the command list.
22
23    -noflatten
24        do not flatten design before synthesis
25

```

```

26     -retime
27         run 'abc' with '-dff -D 1' options
28
29
30 The following commands are executed by this synthesis command:
31
32     begin:
33         read_verilog -lib +/greenpak4/cells_sim.v
34         hierarchy -check -top <top>
35
36     flatten:      (unless -noflatten)
37         proc
38         flatten
39         tribuf -logic
40
41     coarse:
42         synth -run coarse
43
44     fine:
45         extract_counter -pout GP_DCOMP,GP_DAC -maxwidth 14
46         clean
47         opt -fast -mux_undef -undriven -fine
48         memory_map
49         opt -undriven -fine
50         techmap -map +/techmap.v -map +/greenpak4/cells_latch.v
51         dfflibmap -prepare -liberty +/greenpak4/gp_dff.lib
52         opt -fast
53         abc -dff -D 1      (only if -retime)
54
55     map_luts:
56         nlutmap -assert -luts 0,6,8,2      (for -part SLG46140V)
57         nlutmap -assert -luts 2,8,16,2     (for -part SLG46620V)
58         nlutmap -assert -luts 2,8,16,2     (for -part SLG46621V)
59         clean
60
61     map_cells:
62         shregmap -tech greenpak4
63         dfflibmap -liberty +/greenpak4/gp_dff.lib
64         dffinit -ff GP_DFF Q INIT
65         dffinit -ff GP_DFFR Q INIT
66         dffinit -ff GP_DFFS Q INIT
67         dffinit -ff GP_DFFSR Q INIT
68         iopadmap -bits -inpad GP_IBUF OUT:IN -outpad GP_OBUF IN:OUT -inoutpad GP_OBUF
69         attrmvp -attr src -attr LOC t:GP_OBUF t:GP_OBUFT t:GP_IOBUF n:*
70         attrmvp -attr src -attr LOC -driven t:GP_IBUF n:*
71         techmap -map +/greenpak4/cells_map.v
72         greenpak4_dffinv
73         clean
74
75     check:
76         hierarchy -check
77         stat
78         check -noinit
79

```

```

80 json:
81     write_json <file-name>

```

## C.185 synth\_ice40 – synthesis for iCE40 FPGAs

```

1     synth_ice40 [options]
2
3 This command runs synthesis for iCE40 FPGAs.
4
5     -device < hx | lp | u >
6         relevant only for '-abc9' flow, optimise timing for the specified device.
7         default: hx
8
9     -top <module>
10        use the specified module as top module
11
12     -blif <file>
13        write the design to the specified BLIF file. writing of an output file
14        is omitted if this parameter is not specified.
15
16     -edif <file>
17        write the design to the specified EDIF file. writing of an output file
18        is omitted if this parameter is not specified.
19
20     -json <file>
21        write the design to the specified JSON file. writing of an output file
22        is omitted if this parameter is not specified.
23
24     -run <from_label>:<to_label>
25        only run the commands between the labels (see below). an empty
26        from label is synonymous to 'begin', and empty to label is
27        synonymous to the end of the command list.
28
29     -noflatten
30        do not flatten design before synthesis
31
32     -retime
33        run 'abc' with '-dff -D 1' options
34
35     -nocarry
36        do not use SB_CARRY cells in output netlist
37
38     -nodffe
39        do not use SB_DFFE* cells in output netlist
40
41     -dfffe_min_ce_use <min_ce_use>
42        do not use SB_DFFE* cells if the resulting CE line would go to less
43        than min_ce_use SB_DFFE* in output netlist
44
45     -nobram
46        do not use SB_RAM40_4K* cells in output netlist
47

```

```

48 -dsp
49     use ice40 UltraPlus DSP cells for large arithmetic
50
51 -noabc
52     use built-in Yosys LUT techmapping instead of abc
53
54 -abc2
55     run two passes of 'abc' for slightly improved logic density
56
57 -vpr
58     generate an output netlist (and BLIF file) suitable for VPR
59     (this feature is experimental and incomplete)
60
61 -abc9
62     use new ABC9 flow (EXPERIMENTAL)
63
64 -flowmap
65     use FlowMap LUT techmapping instead of abc (EXPERIMENTAL)
66
67

```

68 The following commands are executed by this synthesis command:

```

69 begin:
70     read_verilog -D ICE40_HX -lib -specify +/ice40/cells_sim.v
71     hierarchy -check -top <top>
72     proc
73
74

```

```

75 flatten:      (unless -noflatten)
76     flatten
77     tribuf -logic
78     deminout
79

```

```

80 coarse:
81     opt_expr
82     opt_clean
83     check
84     opt
85     wreduce
86     peepopt
87     opt_clean
88     share
89     techmap -map +/cmp2lut.v -D LUT_WIDTH=4
90     opt_expr
91     opt_clean
92     memory_dff
93     wreduce t:$mul
94     techmap -map +/mul2dsp.v -map +/ice40/dsp_map.v -D DSP_A_MAXWIDTH=16

```

```

95 (if -dsp) select a:mul2dsp (if -dsp)
96 setattr -unset mul2dsp (if -dsp)
97 opt_expr -fine (if -dsp)
98 wreduce (if -dsp)
99 select -clear (if -dsp)
100 ice40_dsp (if -dsp)

```

```

101     chtype -set $mul t:$__soft_mul      (if -dsp)
102     alumacc
103     opt
104     fsm
105     opt -fast
106     memory -nomap
107     opt_clean
108
109 map_bram:      (skip if -nobram)
110     memory_bram -rules +/ice40/brams.txt
111     techmap -map +/ice40/brams_map.v
112     ice40_braminit
113
114 map_ffram:
115     opt -fast -mux_undef -undriven -fine
116     memory_map -iattr -attr !ram_block -attr !rom_block -attr logic_block -attr sy
117     opt -undriven -fine
118
119 map_gates:
120     ice40_wrapcarry
121     techmap -map +/techmap.v -map +/ice40/arith_map.v
122     opt -fast
123     abc -dff -D 1      (only if -retime)
124     ice40_opt
125
126 map_ffs:
127     dff2dfffe -direct-match $_DFF_*
128     techmap -D NO_LUT -D NO_ADDER -map +/ice40/cells_map.v
129     opt_expr -mux_undef
130     simplemap
131     ice40_ffinit
132     ice40_ffssr
133     ice40_opt -full
134
135 map_luts:
136     abc      (only if -abc2)
137     ice40_opt (only if -abc2)
138     techmap -map +/ice40/latches_map.v
139     simplemap                                     (if -noabc or -flowmap)
140     techmap -map +/gate2lut.v -D LUT_WIDTH=4      (only if -noabc)
141     flowmap -maxlut 4      (only if -flowmap)
142     abc -dress -lut 4      (skip if -noabc)
143     ice40_wrapcarry -unwrap
144     techmap -D NO_LUT -map +/ice40/cells_map.v
145     clean
146     opt_lut -dlogic SB_CARRY:I0=2:I1=1:CI=0
147
148 map_cells:
149     techmap -map +/ice40/cells_map.v      (with -D NO_LUT in vpr mode)
150     clean
151
152 check:
153     autaname
154     hierarchy -check

```

```

155     stat
156     check -noinit
157
158   blif:
159     opt_clean -purge                                (vpr mode)
160     write_blif -attr -cname -conn -param <file-name> (vpr mode)
161     write_blif -gates -attr -param <file-name>      (non-vpr mode)
162
163   edif:
164     write_edif <file-name>
165
166   json:
167     write_json <file-name>

```

### C.186 synth\_intel – synthesis for Intel (Altera) FPGAs.

```

1   synth_intel [options]
2
3   This command runs synthesis for Intel FPGAs.
4
5   -family <max10 | arria10gx | cyclone10lp | cyclonev | cycloneiv | cycloneive>
6       generate the synthesis netlist for the specified family.
7       MAX10 is the default target if no family argument specified.
8       For Cyclone IV GX devices, use cycloneiv argument; for Cyclone IV E, use cycloneive
9       Cyclone V and Arria 10 GX devices are experimental.
10
11  -top <module>
12      use the specified module as top module (default='top')
13
14  -vqm <file>
15      write the design to the specified Verilog Quartus Mapping File. Writing of an
16      output file is omitted if this parameter is not specified.
17      Note that this backend has not been tested and is likely incompatible
18      with recent versions of Quartus.
19
20  -vpr <file>
21      write BLIF files for VPR flow experiments. The synthesized BLIF output file is
22      compatible with the Quartus flow. Writing of an
23      output file is omitted if this parameter is not specified.
24
25  -run <from_label>:<to_label>
26      only run the commands between the labels (see below). an empty
27      from label is synonymous to 'begin', and empty to label is
28      synonymous to the end of the command list.
29
30  -iopads
31      use IO pad cells in output netlist
32
33  -nobram
34      do not use block RAM cells in output netlist
35
36  -noflatten

```

```

37     do not flatten design before synthesis
38
39     -retime
40         run 'abc' with '-dff -D 1' options
41
42 The following commands are executed by this synthesis command:
43
44     begin:
45
46     family:
47         read_verilog -sv -lib +/intel/max10/cells_sim.v
48         read_verilog -sv -lib +/intel/common/m9k_bb.v
49         read_verilog -sv -lib +/intel/common/altp11_bb.v
50         hierarchy -check -top <top>
51
52     flatten:      (unless -noflatten)
53         proc
54         flatten
55         tribuf -logic
56         deminout
57
58     coarse:
59         synth -run coarse
60
61     map_bram:      (skip if -nobram)
62         memory_bram -rules +/intel/common/brams_m9k.txt      (if applicable for family)
63         techmap -map +/intel/common/brams_map_m9k.v          (if applicable for family)
64
65     map_ffram:
66         opt -fast -mux_undef -undriven -fine -full
67         memory_map
68         opt -undriven -fine
69         dff2dfffe -direct-match $_DFF_*
70         opt -fine
71         techmap -map +/techmap.v
72         opt -full
73         clean -purge
74         setundef -undriven -zero
75         abc -markgroups -dff -D 1      (only if -retime)
76
77     map_luts:
78         abc -lut 4
79         clean
80
81     map_cells:
82         iopadmap -bits -outpad $__outpad I:O -inpad $__inpad O:I      (if -iopads)
83         techmap -map +/intel/max10/cells_map.v
84         dffinit -highlow -ff dffeas q power_up
85         clean -purge
86
87     check:
88         hierarchy -check
89         stat
90         check -noinit

```

```

91
92     vqm:
93         write_verilog -attr2comment -defparam -nohex -decimal -renameprefix syn_ <file>
94
95     vpr:
96         opt_clean -purge
97         write_blif <file-name>
98
99
100 WARNING: THE 'synth_intel' COMMAND IS EXPERIMENTAL.

```

## C.187 synth\_sf2 – synthesis for SmartFusion2 and IGLOO2 FPGAs

```

1     synth_sf2 [options]
2
3 This command runs synthesis for SmartFusion2 and IGLOO2 FPGAs.
4
5     -top <module>
6         use the specified module as top module
7
8     -edif <file>
9         write the design to the specified EDIF file. writing of an output file
10        is omitted if this parameter is not specified.
11
12    -vlog <file>
13        write the design to the specified Verilog file. writing of an output file
14        is omitted if this parameter is not specified.
15
16    -json <file>
17        write the design to the specified JSON file. writing of an output file
18        is omitted if this parameter is not specified.
19
20    -run <from_label>:<to_label>
21        only run the commands between the labels (see below). an empty
22        from label is synonymous to 'begin', and empty to label is
23        synonymous to the end of the command list.
24
25    -noflatten
26        do not flatten design before synthesis
27
28    -noiobs
29        run synthesis in "block mode", i.e. do not insert IO buffers
30
31    -clkbuf
32        insert direct PAD->global_net buffers
33
34    -retime
35        run 'abc' with '-dff -D 1' options
36
37
38 The following commands are executed by this synthesis command:
39

```



```

40 begin:
41     read_verilog -lib +/sf2/cells_sim.v
42     hierarchy -check -top <top>
43
44 flatten:      (unless -noflatten)
45     proc
46     flatten
47     tribuf -logic
48     deminout
49
50 coarse:
51     synth -run coarse
52
53 fine:
54     opt -fast -mux_undef -undriven -fine
55     memory_map
56     opt -undriven -fine
57     techmap -map +/techmap.v -map +/sf2/arith_map.v
58     opt -fast
59     abc -dff -D 1      (only if -retime)
60
61 map_ffs:
62     techmap -D NO_LUT -map +/sf2/cells_map.v
63     opt_expr -mux_undef
64     simplemap
65
66 map_luts:
67     abc -lut 4
68     clean
69
70 map_cells:
71     techmap -map +/sf2/cells_map.v
72     clean
73
74 map_iobs:
75     sf2_iobs [-clkbuff]      (unless -noioobs)
76     clean
77
78 check:
79     hierarchy -check
80     stat
81     check -noinit
82
83 edif:
84     write_edif -gndvccy <file-name>
85
86 vlog:
87     write_verilog <file-name>
88
89 json:
90     write_json <file-name>

```

**C.188 synth\_xilinx – synthesis for Xilinx FPGAs**

```

1 synth_xilinx [options]
2
3 This command runs synthesis for Xilinx FPGAs. This command does not operate on
4 partly selected designs. At the moment this command creates netlists that are
5 compatible with 7-Series Xilinx devices.
6
7 -top <module>
8     use the specified module as top module
9
10 -family <family>
11     run synthesis for the specified Xilinx architecture
12     generate the synthesis netlist for the specified family.
13     supported values:
14     - xcup: Ultrascale Plus
15     - xcu: Ultrascale
16     - xc7: Series 7 (default)
17     - xc6s: Spartan 6
18     - xc6v: Virtex 6
19     - xc5v: Virtex 5 (EXPERIMENTAL)
20     - xc4v: Virtex 4 (EXPERIMENTAL)
21     - xc3sda: Spartan 3A DSP (EXPERIMENTAL)
22     - xc3sa: Spartan 3A (EXPERIMENTAL)
23     - xc3se: Spartan 3E (EXPERIMENTAL)
24     - xc3s: Spartan 3 (EXPERIMENTAL)
25     - xc2vp: Virtex 2 Pro (EXPERIMENTAL)
26     - xc2v: Virtex 2 (EXPERIMENTAL)
27     - xcve: Virtex E, Spartan 2E (EXPERIMENTAL)
28     - xcv: Virtex, Spartan 2 (EXPERIMENTAL)
29
30 -edif <file>
31     write the design to the specified edif file. writing of an output file
32     is omitted if this parameter is not specified.
33
34 -blif <file>
35     write the design to the specified BLIF file. writing of an output file
36     is omitted if this parameter is not specified.
37
38 -vpr
39     generate an output netlist (and BLIF file) suitable for VPR
40     (this feature is experimental and incomplete)
41
42 -ise
43     generate an output netlist suitable for ISE
44
45 -nobram
46     do not use block RAM cells in output netlist
47
48 -nolutram
49     do not use distributed RAM cells in output netlist
50
51 -nosrl
52     do not use distributed SRL cells in output netlist

```

```

53
54 -nocarry
55     do not use XORCY/MUXCY/CARRY4 cells in output netlist
56
57 -nowidelut
58     do not use MUXF[5-9] resources to implement LUTs larger than native for the target
59
60 -nodsp
61     do not use DSP48*s to implement multipliers and associated logic
62
63 -noiopad
64     disable I/O buffer insertion (useful for hierarchical or
65     out-of-context flows)
66
67 -noclkbuf
68     disable automatic clock buffer insertion
69
70 -uram
71     infer URAM288s for large memories (xcup only)
72
73 -widemux <int>
74     enable inference of hard multiplexer resources (MUXF[78]) for muxes at or
75     above this number of inputs (minimum value 2, recommended value >= 5).
76     default: 0 (no inference)
77
78 -run <from_label>:<to_label>
79     only run the commands between the labels (see below). an empty
80     from label is synonymous to 'begin', and empty to label is
81     synonymous to the end of the command list.
82
83 -flatten
84     flatten design before synthesis
85
86 -dff
87     run 'abc'/'abc9' with -dff option
88
89 -retime
90     run 'abc' with '-D 1' option to enable flip-flop retiming.
91     implies -dff.
92
93 -abc9
94     use new ABC9 flow (EXPERIMENTAL)
95
96

```

The following commands are executed by this synthesis command:

```

98
99 begin:
100     read_verilog -lib -specify +/xilinx/cells_sim.v
101     read_verilog -lib +/xilinx/cells_xtra.v
102     hierarchy -check -auto-top
103
104 prepare:
105     proc
106     flatten    (with '-flatten')

```

```

107     tribuf -logic
108     deminout
109     opt_expr
110     opt_clean
111     check
112     opt
113     wreduce [-keepdc]      (option for '-widemux')
114     peepopt
115     opt_clean
116     muxpack      ('-widemux' only)
117     pmux2shiftx   (skip if '-nosrl' and '-widemux=0')
118     clean         (skip if '-nosrl' and '-widemux=0')
119
120 map_dsp:      (skip if '-nodsp')
121     memory_dff
122     techmap -map +/mul2dsp.v -map +/xilinx/{family}_dsp_map.v {options}
123     select a:mul2dsp
124     setattr -unset mul2dsp
125     opt_expr -fine
126     wreduce
127     select -clear
128     xilinx_dsp -family <family>
129     chtype -set $mul t:$__soft_mul
130
131 coarse:
132     techmap -map +/cmp2lut.v -map +/cmp2lcu.v -D LUT_WIDTH=[46]
133     alumacc
134     share
135     opt
136     fsm
137     opt -fast
138     memory -nomap
139     opt_clean
140
141 map_uram:      (only if '-uram')
142     memory_bram -rules +/xilinx/{family}_urams.txt
143     techmap -map +/xilinx/{family}_urams_map.v
144
145 map_bram:      (skip if '-nobram')
146     memory_bram -rules +/xilinx/{family}_brams.txt
147     techmap -map +/xilinx/{family}_brams_map.v
148
149 map_lutram:    (skip if '-nolutram')
150     memory_bram -rules +/xilinx/lut[46]_lutrams.txt
151     techmap -map +/xilinx/lutrams_map.v
152
153 map_ffram:
154     simplemap t:$dff t:$adff t:$mux
155     dff2dffs [-match-init]      (-match-init for xc6s only)
156     opt -fast -full
157     memory_map
158
159 fine:
160     dff2dfffe -direct-match $__DFF_* -direct-match $__DFFS_*

```

```

161     muxcover <internal options> ('-widemux' only)
162     opt -full
163     xilinx_srl -variable -minlen 3      (skip if '-nosrl')
164     techmap -map +/techmap.v -D LUT_SIZE=[46] [-map +/xilinx/mux_map.v] -map +/xi
165     opt -fast
166
167     map_cells:
168     iopadmap -bits -outpad OBUF I:O -inpad IBUF O:I -toutpad $__XILINX_TOUTPAD OE:
(skip if '-noiopad')
169     techmap -map +/techmap.v -map +/xilinx/cells_map.v
170     clean
171
172     map_ffs:
173     techmap -map +/xilinx/{family}_ff_map.v      ('-abc9' only)
174
175     map_luts:
176     opt_expr -mux_undef
177     abc -luts 2:2,3,6:5[,10,20] [-dff] [-D 1]      (option for 'nowidelut', '-dff',
178     clean
179     xilinx_srl -fixed -minlen 3      (skip if '-nosrl')
180     techmap -map +/xilinx/lut_map.v -map +/xilinx/cells_map.v -map +/xilinx/{famil
181     xilinx_dffopt [-lut4]
182     opt_lut_ins -tech xilinx
183
184     finalize:
185     clkbufmap -buf BUFG O:I      (skip if '-noclkbuf')
186     extractinv -inv INV O:I      (only if '-ise')
187     clean
188
189     check:
190     hierarchy -check
191     stat -tech xilinx
192     check -noinit
193
194     edif:
195     write_edif -pvector bra
196
197     blif:
198     write_blif

```

## C.189 tcl – execute a TCL script file

```

1     tcl <filename> [args]
2
3     This command executes the tcl commands in the specified file.
4     Use 'yosys cmd' to run the yosys command 'cmd' from tcl.
5
6     The tcl command 'yosys -import' can be used to import all yosys
7     commands directly as tcl commands to the tcl shell. Yosys commands
8     'proc' and 'rename' are wrapped to tcl commands 'procs' and 'renames'
9     in order to avoid a name collision with the built in commands.
10

```

11 If any arguments are specified, these arguments are provided to the script via  
 12 the standard \$argc and \$argv variables.

## C.190 techmap – generic technology mapper

```

1  techmap [-map filename] [selection]
2
3  This pass implements a very simple technology mapper that replaces cells in
4  the design with implementations given in form of a Verilog or ilang source
5  file.
6
7  -map filename
8      the library of cell implementations to be used.
9      without this parameter a builtin library is used that
10     transforms the internal RTL cells to the internal gate
11     library.
12
13  -map %<design-name>
14     like -map above, but with an in-memory design instead of a file.
15
16  -extern
17     load the cell implementations as separate modules into the design
18     instead of inlining them.
19
20  -max_iter <number>
21     only run the specified number of iterations on each module.
22     default: unlimited
23
24  -recursive
25     instead of the iterative breadth-first algorithm use a recursive
26     depth-first algorithm. both methods should yield equivalent results,
27     but may differ in performance.
28
29  -autoproc
30     Automatically call "proc" on implementations that contain processes.
31
32  -wb
33     Ignore the 'whitebox' attribute on cell implementations.
34
35  -assert
36     this option will cause techmap to exit with an error if it can't map
37     a selected cell. only cell types that end on an underscore are accepted
38     as final cell types by this mode.
39
40  -D <define>, -I <incdir>
41     this options are passed as-is to the Verilog frontend for loading the
42     map file. Note that the Verilog frontend is also called with the
43     '-nooverwrite' option set.
44
45  When a module in the map file has the 'techmap_celltype' attribute set, it will
46  match cells with a type that match the text value of this attribute. Otherwise
47  the module name will be used to match the cell.

```

When a module in the map file has the 'techmap\_simplemap' attribute set, techmap will use 'simplemap' (see 'help simplemap') to map cells matching the module.

When a module in the map file has the 'techmap\_maccmap' attribute set, techmap will use 'maccmap' (see 'help maccmap') to map cells matching the module.

When a module in the map file has the 'techmap\_wrap' attribute set, techmap will create a wrapper for the cell and then run the command string that the attribute is set to on the wrapper module.

When a port on a module in the map file has the 'techmap\_autopurge' attribute set, and that port is not connected in the instantiation that is mapped, then a cell port connected only to such wires will be omitted in the mapped version of the circuit.

All wires in the modules from the map file matching the pattern `_TECHMAP_*` or `*._TECHMAP_*` are special wires that are used to pass instructions from the mapping module to the techmap command. At the moment the following special wires are supported:

#### `_TECHMAP_FAIL_`

When this wire is set to a non-zero constant value, techmap will not use this module and instead try the next module with a matching 'techmap\_celltype' attribute.

When such a wire exists but does not have a constant value after all `_TECHMAP_DO_*` commands have been executed, an error is generated.

#### `_TECHMAP_DO_*`

This wires are evaluated in alphabetical order. The constant text value of this wire is a yosys command (or sequence of commands) that is run by techmap on the module. A common use case is to run 'proc' on modules that are written using always-statements.

When such a wire has a non-constant value at the time it is to be evaluated, an error is produced. That means it is possible for such a wire to start out as non-constant and evaluate to a constant value during processing of other `_TECHMAP_DO_*` commands.

A `_TECHMAP_DO_*` command may start with the special token 'CONSTMAP; '. In this case techmap will create a copy for each distinct configuration of constant inputs and shorted inputs at this point and import the constant and connected bits into the map module. All further commands are executed in this copy. This is a very convenient way of creating optimized specializations of techmap modules without using the special parameters described below.

A `_TECHMAP_DO_*` command may start with the special token 'RECURSION; '. Then techmap will recursively replace the cells in the module with their implementation. This is not affected by the `-max_iter` option.

It is possible to combine both prefixes to 'RECURSION; CONSTMAP; '.

`_TECHMAP_REMOVEINIT_<port-name>_`

When this wire is set to a constant value, the init attribute of the wire(s) connected to this port will be consumed. This wire must have the same width as the given port, and for every bit that is set to 1 in the value, the corresponding init attribute bit will be changed to 1'bx. If all bits of an init attribute are left as x, it will be removed.

In addition to this special wires, techmap also supports special parameters in modules in the map file:

`_TECHMAP_CELLTYPE_`

When a parameter with this name exists, it will be set to the type name of the cell that matches the module.

`_TECHMAP_CONSTMSK_<port-name>_`

`_TECHMAP_CONSTVAL_<port-name>_`

When this pair of parameters is available in a module for a port, then former has a 1-bit for each constant input bit and the latter has the value for this bit. The unused bits of the latter are set to undef (x).

`_TECHMAP_WIREINIT_<port-name>_`

When a parameter with this name exists, it will be set to the initial value of the wire(s) connected to the given port, as specified by the init attribute. If the attribute doesn't exist, x will be filled for the missing bits. To remove the init attribute bits used, use the `_TECHMAP_REMOVEINIT_*_` wires.

`_TECHMAP_BITS_CONNMAP_`

`_TECHMAP_CONNMAP_<port-name>_`

For an N-bit port, the `_TECHMAP_CONNMAP_<port-name>_` parameter, if it exists, will be set to an `N*_TECHMAP_BITS_CONNMAP_` bit vector containing N words (of `_TECHMAP_BITS_CONNMAP_` bits each) that assign each single bit driver a unique id. The values 0-3 are reserved for 0, 1, x, and z. This can be used to detect shorted inputs.

When a module in the map file has a parameter where the according cell in the design has a port, the module from the map file is only used if the port in the design is connected to a constant value. The parameter is then set to the constant value.

A cell with the name `_TECHMAP_REPLACE_` in the map file will inherit the name and attributes of the cell that is being replaced.

A cell with a name of the form `'_TECHMAP_REPLACE_<suffix>'` in the map file will be named thus but with the `'_TECHMAP_REPLACE_'` prefix substituted with the name of the cell being replaced.

Similarly, a wire named in the form `'_TECHMAP_REPLACE_<suffix>'` will cause a new wire alias to be created and named as above but with the `'_TECHMAP_REPLACE_'` prefix also substituted.

See 'help extract' for a pass that does the opposite thing.

See 'help flatten' for a pass that does flatten the design (which is essentially techmap but using the design itself as map library).



**C.191 tee – redirect command output to file**

```

1      tee [-q] [-o logfile|-a logfile] cmd
2
3  Execute the specified command, optionally writing the commands output to the
4  specified logfile(s).
5
6      -q
7          Do not print output to the normal destination (console and/or log file).
8
9      -o logfile
10         Write output to this file, truncate if exists.
11
12      -a logfile
13         Write output to this file, append if exists.
14
15      +INT, -INT
16         Add/subtract INT from the -v setting for this command.

```

**C.192 test\_abclloop – automatically test handling of loops in abc command**

```

1      test_abclloop [options]
2
3  Test handling of logic loops in ABC.
4
5      -n {integer}
6          create this number of circuits and test them (default = 100).
7
8      -s {positive_integer}
9          use this value as rng seed value (default = unix time).

```

**C.193 test\_autotb – generate simple test benches**

```

1      test_autotb [options] [filename]
2
3  Automatically create primitive Verilog test benches for all modules in the
4  design. The generated testbenches toggle the input pins of the module in
5  a semi-random manner and dumps the resulting output signals.
6
7  This can be used to check the synthesis results for simple circuits by
8  comparing the testbench output for the input files and the synthesis results.
9
10 The backend automatically detects clock signals. Additionally a signal can
11 be forced to be interpreted as clock signal by setting the attribute
12 'gentb_clock' on the signal.
13
14 The attribute 'gentb_constant' can be used to force a signal to a constant
15 value after initialization. This can e.g. be used to force a reset signal

```

```

16 low in order to explore more inner states in a state machine.
17
18 The attribute 'gentb_skip' can be attached to modules to suppress testbench
19 generation.
20
21     -n <int>
22         number of iterations the test bench should run (default = 1000)
23
24     -seed <int>
25         seed used for pseudo-random number generation (default = 0).
26         a value of 0 will cause an arbitrary seed to be chosen, based on
27         the current system time.

```

### C.194 test\_cell – automatically test the implementation of a cell type

```

1     test_cell [options] {cell-types}
2
3 Tests the internal implementation of the given cell type (for example '$add')
4 by comparing SAT solver, EVAL and TECHMAP implementations of the cell types..
5
6 Run with 'all' instead of a cell type to run the test on all supported
7 cell types. Use for example 'all /$add' for all cell types except $add.
8
9     -n {integer}
10         create this number of cell instances and test them (default = 100).
11
12     -s {positive_integer}
13         use this value as rng seed value (default = unix time).
14
15     -f {ilang_file}
16         don't generate circuits. instead load the specified ilang file.
17
18     -w {filename_prefix}
19         don't test anything. just generate the circuits and write them
20         to ilang files with the specified prefix
21
22     -map {filename}
23         pass this option to techmap.
24
25     -simlib
26         use "techmap -D SIMLIB_NOCHECKS -map +/simlib.v -max_iter 2 -autoproc"
27
28     -aigmap
29         instead of calling "techmap", call "aigmap"
30
31     -muxdiv
32         when creating test benches with dividers, create an additional mux
33         to mask out the division-by-zero case
34
35     -script {script_file}
36         instead of calling "techmap", call "script {script_file}".
37

```

```

38  -const
39      set some input bits to random constant values
40
41  -nosat
42      do not check SAT model or run SAT equivalence checking
43
44  -noeval
45      do not check const-eval models
46
47  -edges
48      test cell edges db creator against sat-based implementation
49
50  -v
51      print additional debug information to the console
52
53  -vlog {filename}
54      create a Verilog test bench to test simlib and write_verilog

```

### C.195 test\_pmgen – test pass for pmgen

```

1  test_pmgen -reduce_chain [options] [selection]
2
3  Demo for recursive pmgen patterns. Map chains of AND/OR/XOR to $reduce_*.
4
5
6  test_pmgen -reduce_tree [options] [selection]
7
8  Demo for recursive pmgen patterns. Map trees of AND/OR/XOR to $reduce_*.
9
10
11 test_pmgen -eqpmux [options] [selection]
12
13 Demo for recursive pmgen patterns. Optimize EQ/NE/PMUX circuits.
14
15
16 test_pmgen -generate [options] <pattern_name>
17
18 Create modules that match the specified pattern.

```

### C.196 torder – print cells in topological order

```

1  torder [options] [selection]
2
3  This command prints the selected cells in topological order.
4
5  -stop <cell_type> <cell_port>
6      do not use the specified cell port in topological sorting
7
8  -noautostop
9      by default Q outputs of internal FF cells and memory read port outputs

```

10 | are not used in topological sorting. this option deactivates that.

### C.197 trace – redirect command output to file

```
1 | trace cmd
2 |
3 | Execute the specified command, logging all changes the command performs on
4 | the design in real time.
```

### C.198 tribuf – infer tri-state buffers

```
1 | tribuf [options] [selection]
2 |
3 | This pass transforms $mux cells with 'z' inputs to tristate buffers.
4 |
5 | -merge
6 |     merge multiple tri-state buffers driving the same net
7 |     into a single buffer.
8 |
9 | -logic
10 |     convert tri-state buffers that do not drive output ports
11 |     to non-tristate logic. this option implies -merge.
```

### C.199 uniquify – create unique copies of modules

```
1 | uniquify [selection]
2 |
3 | By default, a module that is instantiated by several other modules is only
4 | kept once in the design. This preserves the original modularity of the design
5 | and reduces the overall size of the design in memory. But it prevents certain
6 | optimizations and other operations on the design. This pass creates unique
7 | modules for all selected cells. The created modules are marked with the
8 | 'unique' attribute.
9 |
10 | This commands only operates on modules that by themselves have the 'unique'
11 | attribute set (the 'top' module is unique implicitly).
```

### C.200 verifc – load Verilog and VHDL designs using Verific

```
1 | verifc {-vlog95|-vlog2k|-sv2005|-sv2009|-sv2012|-sv} <verilog-file>..
2 |
3 | Load the specified Verilog/SystemVerilog files into Verific.
4 |
5 | All files specified in one call to this command are one compilation unit.
6 | Files passed to different calls to this command are treated as belonging to
```

```

7 different compilation units.
8
9 Additional -D<macro>[=<value>] options may be added after the option indicating
10 the language version (and before file names) to set additional verilog defines.
11 The macros SYNTHESIS and VERIFIC are defined implicitly.
12
13
14     verific -formal <verilog-file>..
15
16 Like -sv, but define FORMAL instead of SYNTHESIS.
17
18
19     verific {-vhd187|-vhd193|-vhd12k|-vhd12008|-vhd1} <vhd1-file>..
20
21 Load the specified VHDL files into Verific.
22
23
24     verific [-work <libname>] {-sv|-vhd1|...} <hdl-file>
25
26 Load the specified Verilog/SystemVerilog/VHDL file into the specified library.
27 (default library when -work is not present: "work")
28
29
30     verific [-L <libname>] {-sv|-vhd1|...} <hdl-file>
31
32 Look up external definitions in the specified library.
33 (-L may be used more than once)
34
35
36     verific -vlog-incdir <directory>..
37
38 Add Verilog include directories.
39
40
41     verific -vlog-libdir <directory>..
42
43 Add Verilog library directories. Verific will search in this directories to
44 find undefined modules.
45
46
47     verific -vlog-define <macro>[=<value>]..
48
49 Add Verilog defines.
50
51
52     verific -vlog-undef <macro>..
53
54 Remove Verilog defines previously set with -vlog-define.
55
56
57     verific -set-error <msg_id>..
58     verific -set-warning <msg_id>..
59     verific -set-info <msg_id>..
60     verific -set-ignore <msg_id>..

```

Set message severity. <msg\_id> is the string in square brackets when a message is printed, such as VERI-1209.

```
verific -import [options] <top-module>..
```

Elaborate the design for the specified top modules, import to Yosys and reset the internal state of Verific.

Import options:

-all

Elaborate all modules, not just the hierarchy below the given top modules. With this option the list of modules to import is optional.

-gates

Create a gate-level netlist.

-flatten

Flatten the design in Verific before importing.

-extnets

Resolve references to external nets by adding module ports as needed.

-autocover

Generate automatic cover statements for all asserts

-fullinit

Keep all register initializations, even those for non-FF registers.

-chparam name value

Elaborate the specified top modules (all modules when -all given) using this parameter value. Modules on which this parameter does not exist will cause Verific to produce a VERI-1928 or VHDL-1676 message. This option can be specified multiple times to override multiple parameters. String values must be passed in double quotes (").

-v, -vv

Verbose log messages. (-vv is even more verbose than -v.)

The following additional import options are useful for debugging the Verific bindings (for Yosys and/or Verific developers):

-k

Keep going after an unsupported verific primitive is found. The unsupported primitive is added as blockbox module to the design. This will also add all SVA related cells to the design parallel to the checker logic inferred by it.

-V

Import Verific netlist as-is without translating to Yosys cell types.

-nosva

```

115     Ignore SVA properties, do not infer checker logic.
116
117     -L <int>
118         Maximum number of ctrl bits for SVA checker FSMs (default=16).
119
120     -n
121         Keep all Verific names on instances and nets. By default only
122         user-declared names are preserved.
123
124     -d <dump_file>
125         Dump the Verific netlist as a verilog file.
126
127
128     Use Symbiotic EDA Suite if you need Yosys+Verific.
129     https://www.symbioticeda.com/seda-suite
130
131     Contact office@symbioticeda.com for free evaluation
132     binaries of Symbiotic EDA Suite.

```

## C.201 verilog\_defaults – set default options for read\_verilog

```

1     verilog_defaults -add [options]
2
3     Add the specified options to the list of default options to read_verilog.
4
5
6     verilog_defaults -clear
7
8     Clear the list of Verilog default options.
9
10
11     verilog_defaults -push
12     verilog_defaults -pop
13
14     Push or pop the list of default options to a stack. Note that -push does
15     not imply -clear.

```

## C.202 verilog\_defines – define and undefine verilog defines

```

1     verilog_defines [options]
2
3     Define and undefine verilog preprocessor macros.
4
5     -Dname[=definition]
6         define the preprocessor symbol 'name' and set its optional value
7         'definition'
8
9     -Uname[=definition]
10        undefine the preprocessor symbol 'name'
11

```

```

12     -reset
13         clear list of defined preprocessor symbols
14
15     -list
16         list currently defined preprocessor symbols

```

### C.203 **wbflip** – flip the whitebox attribute

```

1     wbflip [selection]
2
3     Flip the whitebox attribute on selected cells. I.e. if it's set, unset it, and
4     vice-versa. Blackbox cells are not effected by this command.

```

### C.204 **wreduce** – reduce the word size of operations if possible

```

1     wreduce [options] [selection]
2
3     This command reduces the word size of operations. For example it will replace
4     the 32 bit adders in the following code with adders of more appropriate widths:
5
6     module test(input [3:0] a, b, c, output [7:0] y);
7         assign y = a + b + c + 1;
8     endmodule
9
10    Options:
11
12    -memx
13        Do not change the width of memory address ports. Use this options in
14        flows that use the 'memory_memx' pass.
15
16    -keepdc
17        Do not optimize explicit don't-care values.

```

### C.205 **write\_aiger** – write design to AIGER file

```

1     write_aiger [options] [filename]
2
3     Write the current design to an AIGER file. The design must be flattened and
4     must not contain any cell types except $_AND_, $_NOT_, simple FF types,
5     $assert and $assume cells, and $initstate cells.
6
7     $assert and $assume cells are converted to AIGER bad state properties and
8     invariant constraints.
9
10    -ascii
11        write ASCII version of AIGER format
12

```



```

13  -zinit
14      convert FFs to zero-initialized FFs, adding additional inputs for
15      uninitialized FFs.
16
17  -miter
18      design outputs are AIGER bad state properties
19
20  -symbols
21      include a symbol table in the generated AIGER file
22
23  -map <filename>
24      write an extra file with port and latch symbols
25
26  -vmap <filename>
27      like -map, but more verbose
28
29  -I, -O, -B, -L
30      If the design contains no input/output/assert/flip-flop then create one
31      dummy input/output/bad_state-pin or latch to make the tools reading the
32      AIGER file happy.

```

## C.206 write\_blif – write design to BLIF file

```

1  write_blif [options] [filename]
2
3  Write the current design to an BLIF file.
4
5  -top top_module
6      set the specified module as design top module
7
8  -buf <cell-type> <in-port> <out-port>
9      use cells of type <cell-type> with the specified port names for buffers
10
11 -unbuf <cell-type> <in-port> <out-port>
12     replace buffer cells with the specified name and port names with
13     a .names statement that models a buffer
14
15 -true <cell-type> <out-port>
16 -false <cell-type> <out-port>
17 -undef <cell-type> <out-port>
18     use the specified cell types to drive nets that are constant 1, 0, or
19     undefined. when '-' is used as <cell-type>, then <out-port> specifies
20     the wire name to be used for the constant signal and no cell driving
21     that wire is generated. when '+' is used as <cell-type>, then <out-port>
22     specifies the wire name to be used for the constant signal and a .names
23     statement is generated to drive the wire.
24
25 -noalias
26     if a net name is aliasing another net name, then by default a net
27     without fanout is created that is driven by the other net. This option
28     suppresses the generation of this nets without fanout.
29

```

30 The following options can be useful when the generated file is not going to be  
 31 read by a BLIF parser but a custom tool. It is recommended to not name the output  
 32 file \*.blif when any of this options is used.

```

33
34 -icells
35     do not translate Yosys's internal gates to generic BLIF logic
36     functions. Instead create .subckt or .gate lines for all cells.
37
38 -gates
39     print .gate instead of .subckt lines for all cells that are not
40     instantiations of other modules from this design.
41
42 -conn
43     do not generate buffers for connected wires. instead use the
44     non-standard .conn statement.
45
46 -attr
47     use the non-standard .attr statement to write cell attributes
48
49 -param
50     use the non-standard .param statement to write cell parameters
51
52 -cname
53     use the non-standard .cname statement to write cell names
54
55 -iname, -iattr
56     enable -cname and -attr functionality for .names statements
57     (the .cname and .attr statements will be included in the BLIF
58     output after the truth table for the .names statement)
59
60 -blackbox
61     write blackbox cells with .blackbox statement.
62
63 -impltf
64     do not write definitions for the $true, $false and $undef wires.
```

## C.207 write\_btor – write design to BTOR file

```

1     write_btor [options] [filename]
2
3 Write a BTOR description of the current design.
4
5 -v
6     Add comments and indentation to BTOR output file
7
8 -s
9     Output only a single bad property for all asserts
10
11 -c
12     Output cover properties using 'bad' statements instead of asserts
13
14 -i <filename>
```

15 Create additional info file with auxiliary information

## C.208 write\_cxxrtl – convert design to C++ RTL simulation

```

1  write_cxxrtl [options] [filename]
2
3  Write C++ code for simulating the design. The generated code requires a driver;
4  the following simple driver is provided as an example:
5
6  #include "top.cc"
7
8  int main() {
9      cxxrtl_design::p_top top;
10     while (1) {
11         top.p_clk.next = value<1> {1u};
12         top.step();
13         top.p_clk.next = value<1> {0u};
14         top.step();
15     }
16 }
17
18 The following options are supported by this backend:
19
20 -O <level>
21     set the optimization level. the default is -O5. higher optimization
22     levels dramatically decrease compile and run time, and highest level
23     possible for a design should be used.
24
25 -O0
26     no optimization.
27
28 -O1
29     elide internal wires if possible.
30
31 -O2
32     like -O1, and localize internal wires if possible.
33
34 -O3
35     like -O2, and elide public wires not marked (*keep*) if possible.
36
37 -O4
38     like -O3, and localize public wires not marked (*keep*) if possible.
39
40 -O5
41     like -O4, and run 'splitnets -driver; opt_clean -purge' first.

```

## C.209 write\_edif – write design to EDIF netlist file

```

1  write_edif [options] [filename]
2

```

```

3 Write the current design to an EDIF netlist file.
4
5     -top top_module
6         set the specified module as design top module
7
8     -nogndvcc
9         do not create "GND" and "VCC" cells. (this will produce an error
10        if the design contains constant nets. use "hilomap" to map to custom
11        constant drivers first)
12
13     -gndvccy
14         create "GND" and "VCC" cells with "Y" outputs. (the default is "G"
15         for "GND" and "P" for "VCC".)
16
17     -attrprop
18         create EDIF properties for cell attributes
19
20     -pvector {par|bra|ang}
21         sets the delimiting character for module port rename clauses to
22         parentheses, square brackets, or angle brackets.
23
24 Unfortunately there are different "flavors" of the EDIF file format. This
25 command generates EDIF files for the Xilinx place&route tools. It might be
26 necessary to make small modifications to this command when a different tool
27 is targeted.

```

### C.210 write\_file – write a text to a file

```

1     write_file [options] output_file [input_file]
2
3 Write the text from the input file to the output file.
4
5     -a
6         Append to output file (instead of overwriting)
7
8
9 Inside a script the input file can also can a here-document:
10
11     write_file hello.txt <<EOT
12     Hello World!
13     EOT

```

### C.211 write\_firrtl – write design to a FIRRTL file

```

1     write_firrtl [options] [filename]
2
3 Write a FIRRTL netlist of the current design.
4 The following commands are executed by this command:
5     pmuxtree

```

**C.212 write\_ilang – write design to ilang file**

```

1  write_ilang [filename]
2
3  Write the current design to an 'ilang' file. (ilang is a text representation
4  of a design in yosys's internal format.)
5
6  -selected
7      only write selected parts of the design.
```

**C.213 write\_intersynth – write design to InterSynth netlist file**

```

1  write_intersynth [options] [filename]
2
3  Write the current design to an 'intersynth' netlist file. InterSynth is
4  a tool for Coarse-Grain Example-Driven Interconnect Synthesis.
5
6  -notypes
7      do not generate celltypes and conntypes commands. i.e. just output
8      the netlists. this is used for postsilicon synthesis.
9
10 -lib <verilog_or_ilang_file>
11     Use the specified library file for determining whether cell ports are
12     inputs or outputs. This option can be used multiple times to specify
13     more than one library.
14
15 -selected
16     only write selected modules. modules must be selected entirely or
17     not at all.
18
19 http://www.clifford.at/intersynth/
```

**C.214 write\_json – write design to a JSON file**

```

1  write_json [options] [filename]
2
3  Write a JSON netlist of the current design.
4
5  -aig
6      include AIG models for the different gate types
7
8  -compat-int
9      emit 32-bit or smaller fully-defined parameter values directly
10     as JSON numbers (for compatibility with old parsers)
11
12
13 The general syntax of the JSON output created by this command is as follows:
14
15 {
```

```

16     "modules": {
17         <module_name>: {
18             "ports": {
19                 <port_name>: <port_details>,
20                 ...
21             },
22             "cells": {
23                 <cell_name>: <cell_details>,
24                 ...
25             },
26             "netnames": {
27                 <net_name>: <net_details>,
28                 ...
29             }
30         }
31     },
32     "models": {
33         ...
34     },
35 }

```

36 Where <port\_details> is:

```

38 {
39     "direction": <"input" | "output" | "inout">,
40     "bits": <bit_vector>
41 }
42
43

```

44 And <cell\_details> is:

```

45 {
46     "hide_name": <1 | 0>,
47     "type": <cell_type>,
48     "parameters": {
49         <parameter_name>: <parameter_value>,
50         ...
51     },
52     "attributes": {
53         <attribute_name>: <attribute_value>,
54         ...
55     },
56     "port_directions": {
57         <port_name>: <"input" | "output" | "inout">,
58         ...
59     },
60     "connections": {
61         <port_name>: <bit_vector>,
62         ...
63     },
64 }
65
66

```

67 And <net\_details> is:

```

68 {
69

```

```

70     "hide_name": <1 | 0>,
71     "bits": <bit_vector>
72 }
73

```

The "hide\_name" fields are set to 1 when the name of this cell or net is automatically created and is likely not of interest for a regular user.

```

77 The "port_directions" section is only included for cells for which the
78 interface is known.
79

```

```

80 Module and cell ports and nets can be single bit wide or vectors of multiple
81 bits. Each individual signal bit is assigned a unique integer. The <bit_vector>
82 values referenced above are vectors of this integers. Signal bits that are
83 connected to a constant driver are denoted as string "0", "1", "x", or
84 "z" instead of a number.
85

```

```

86 Bit vectors (including integers) are written as string holding the binary representation
87

```

```

88 For example the following Verilog code:
89

```

```

90     module test(input x, y);
91         (* keep *) foo #(.P(42), .Q(1337))
92             foo_inst (.A({x, y}), .B({y, x}), .C({4'd10, {4{x}})));
93     endmodule
94

```

```

95 Translates to the following JSON output:
96

```

```

97     {
98         "modules": {
99             "test": {
100                 "ports": {
101                     "x": {
102                         "direction": "input",
103                         "bits": [ 2 ]
104                     },
105                     "y": {
106                         "direction": "input",
107                         "bits": [ 3 ]
108                     }
109                 },
110                 "cells": {
111                     "foo_inst": {
112                         "hide_name": 0,
113                         "type": "foo",
114                         "parameters": {
115                             "Q": 1337,
116                             "P": 42
117                         },
118                         "attributes": {
119                             "keep": 1,
120                             "src": "test.v:2"
121                         },
122                         "connections": {
123                             "C": [ 2, 2, 2, 2, "0", "1", "0", "1" ],

```

```

124         "B": [ 2, 3 ],
125         "A": [ 3, 2 ]
126     }
127 }
128 },
129 "netnames": {
130     "y": {
131         "hide_name": 0,
132         "bits": [ 3 ],
133         "attributes": {
134             "src": "test.v:1"
135         }
136     },
137     "x": {
138         "hide_name": 0,
139         "bits": [ 2 ],
140         "attributes": {
141             "src": "test.v:1"
142         }
143     }
144 }
145 }
146 }
147 }

```

The models are given as And-Inverter-Graphs (AIGs) in the following form:

```

151 "models": {
152     <model_name>: [
153         /* 0 */ [ <node-spec> ],
154         /* 1 */ [ <node-spec> ],
155         /* 2 */ [ <node-spec> ],
156         ...
157     ],
158     ...
159 },

```

The following node-types may be used:

```

162 [ "port", <portname>, <bitindex>, <out-list> ]
163     - the value of the specified input port bit
164
165 [ "nport", <portname>, <bitindex>, <out-list> ]
166     - the inverted value of the specified input port bit
167
168 [ "and", <node-index>, <node-index>, <out-list> ]
169     - the ANDed value of the specified nodes
170
171 [ "nand", <node-index>, <node-index>, <out-list> ]
172     - the inverted ANDed value of the specified nodes
173
174 [ "true", <out-list> ]
175     - the constant value 1
176
177

```



```

178     [ "false", <out-list> ]
179     - the constant value 0
180
181 All nodes appear in topological order. I.e. only nodes with smaller indices
182 are referenced by "and" and "nand" nodes.
183
184 The optional <out-list> at the end of a node specification is a list of
185 output portname and bitindex pairs, specifying the outputs driven by this node.
186
187 For example, the following is the model for a 3-input 3-output $reduce_and cell
188 inferred by the following code:
189
190     module test(input [2:0] in, output [2:0] out);
191         assign in = &out;
192     endmodule
193
194     "$reduce_and:3U:3": [
195         /* 0 */ [ "port", "A", 0 ],
196         /* 1 */ [ "port", "A", 1 ],
197         /* 2 */ [ "and", 0, 1 ],
198         /* 3 */ [ "port", "A", 2 ],
199         /* 4 */ [ "and", 2, 3, "Y", 0 ],
200         /* 5 */ [ "false", "Y", 1, "Y", 2 ]
201     ]
202
203 Future version of Yosys might add support for additional fields in the JSON
204 format. A program processing this format must ignore all unknown fields.

```

## C.215 write\_simplec – convert design to simple C code

```

1     write_simplec [options] [filename]
2
3 Write simple C code for simulating the design. The C code written can be used to
4 simulate the design in a C environment, but the purpose of this command is to
5 generate code that works well with C-based formal verification.
6
7     -verbose
8         this will print the recursive walk used to export the modules.
9
10    -i8, -i16, -i32, -i64
11        set the maximum integer bit width to use in the generated code.
12
13 THIS COMMAND IS UNDER CONSTRUCTION

```

## C.216 write\_smt2 – write design to SMT-LIBv2 file

```

1     write_smt2 [options] [filename]
2
3 Write a SMT-LIBv2 [1] description of the current design. For a module with name
4 '<mod>' this will declare the sort '<mod>_s' (state of the module) and will

```

```

5 | define and declare functions operating on that state.
6 |
7 | The following SMT2 functions are generated for a module with name '<mod>'.
8 | Some declarations/definitions are printed with a special comment. A prover
9 | using the SMT2 files can use those comments to collect all relevant metadata
10 | about the design.
11 |
12 |   ; yosys-smt2-module <mod>
13 |   (declare-sort |<mod>_s| 0)
14 |       The sort representing a state of module <mod>.
15 |
16 |   (define-fun |<mod>_h| ((state |<mod>_s|)) Bool (...))
17 |       This function must be asserted for each state to establish the
18 |       design hierarchy.
19 |
20 |   ; yosys-smt2-input <wirename> <width>
21 |   ; yosys-smt2-output <wirename> <width>
22 |   ; yosys-smt2-register <wirename> <width>
23 |   ; yosys-smt2-wire <wirename> <width>
24 |   (define-fun |<mod>_n <wirename>| (|<mod>_s|) (_ BitVec <width>))
25 |   (define-fun |<mod>_n <wirename>| (|<mod>_s|) Bool)
26 |       For each port, register, and wire with the 'keep' attribute set an
27 |       accessor function is generated. Single-bit wires are returned as Bool,
28 |       multi-bit wires as BitVec.
29 |
30 |   ; yosys-smt2-cell <submod> <instancename>
31 |   (declare-fun |<mod>_h <instancename>| (|<mod>_s|) |<submod>_s|)
32 |       There is a function like that for each hierarchical instance. It
33 |       returns the sort that represents the state of the sub-module that
34 |       implements the instance.
35 |
36 |   (declare-fun |<mod>_is| (|<mod>_s|) Bool)
37 |       This function must be asserted 'true' for initial states, and 'false'
38 |       otherwise.
39 |
40 |   (define-fun |<mod>_i| ((state |<mod>_s|)) Bool (...))
41 |       This function must be asserted 'true' for initial states. For
42 |       non-initial states it must be left unconstrained.
43 |
44 |   (define-fun |<mod>_t| ((state |<mod>_s|) (next_state |<mod>_s|)) Bool (...))
45 |       This function evaluates to 'true' if the states 'state' and
46 |       'next_state' form a valid state transition.
47 |
48 |   (define-fun |<mod>_a| ((state |<mod>_s|)) Bool (...))
49 |       This function evaluates to 'true' if all assertions hold in the state.
50 |
51 |   (define-fun |<mod>_u| ((state |<mod>_s|)) Bool (...))
52 |       This function evaluates to 'true' if all assumptions hold in the state.
53 |
54 |   ; yosys-smt2-assert <id> <filename:linenum>
55 |   (define-fun |<mod>_a <id>| ((state |<mod>_s|)) Bool (...))
56 |       Each $assert cell is converted into one of this functions. The function
57 |       evaluates to 'true' if the assert statement holds in the state.
58 |

```

```

59 ; yosys-smt2-assume <id> <filename:linenum>
60 (define-fun |<mod>_u <id>| ((state |<mod>_s|)) Bool (...))
61     Each $assume cell is converted into one of this functions. The function
62     evaluates to 'true' if the assume statement holds in the state.
63 
```

```

64 ; yosys-smt2-cover <id> <filename:linenum>
65 (define-fun |<mod>_c <id>| ((state |<mod>_s|)) Bool (...))
66     Each $cover cell is converted into one of this functions. The function
67     evaluates to 'true' if the cover statement is activated in the state.
68 
```

#### Options:

```

70 -verbose
71     this will print the recursive walk used to export the modules.
72
73 -stbv
74     Use a BitVec sort to represent a state instead of an uninterpreted
75     sort. As a side-effect this will prevent use of arrays to model
76     memories.
77
78 -stdt
79     Use SMT-LIB 2.6 style datatypes to represent a state instead of an
80     uninterpreted sort.
81
82 -nobv
83     disable support for BitVec (FixedSizeBitVectors theory). without this
84     option multi-bit wires are represented using the BitVec sort and
85     support for coarse grain cells (incl. arithmetic) is enabled.
86
87 -nomem
88     disable support for memories (via ArraysEx theory). this option is
89     implied by -nobv. only $mem cells without merged registers in
90     read ports are supported. call "memory" with -nordff to make sure
91     that no registers are merged into $mem read ports. '<mod>_m' functions
92     will be generated for accessing the arrays that are used to represent
93     memories.
94
95 -wires
96     create '<mod>_n' functions for all public wires. by default only ports,
97     registers, and wires with the 'keep' attribute are exported.
98
99 -tpl <template_file>
100     use the given template file. the line containing only the token '%%'
101     is replaced with the regular output of this command.
102 
```

[1] For more information on SMT-LIBv2 visit <http://smt-lib.org/> or read David R. Cok's tutorial: <http://www.grammatech.com/resources/smt/SMTLIBTutorial.pdf>

#### Example:

Consider the following module (test.v). We want to prove that the output can never transition from a non-zero value to a zero value.

```

113
114     module test(input clk, output reg [3:0] y);
115         always @(posedge clk)
116             y <= (y << 1) | ^y;
117     endmodule
118
119 For this proof we create the following template (test.tpl).
120
121     ; we need QF_UFBV for this proof
122     (set-logic QF_UFBV)
123
124     ; insert the auto-generated code here
125     %%
126
127     ; declare two state variables s1 and s2
128     (declare-fun s1 () test_s)
129     (declare-fun s2 () test_s)
130
131     ; state s2 is the successor of state s1
132     (assert (test_t s1 s2))
133
134     ; we are looking for a model with y non-zero in s1
135     (assert (distinct (|test_n y| s1) #b0000))
136
137     ; we are looking for a model with y zero in s2
138     (assert (= (|test_n y| s2) #b0000))
139
140     ; is there such a model?
141     (check-sat)
142
143 The following yosys script will create a 'test.smt2' file for our proof:
144
145     read_verilog test.v
146     hierarchy -check; proc; opt; check -assert
147     write_smt2 -bv -tpl test.tpl test.smt2
148
149 Running 'cvc4 test.smt2' will print 'unsat' because y can never transition
150 from non-zero to zero in the test design.

```

## C.217 write\_smv – write design to SMV file

```

1     write_smv [options] [filename]
2
3 Write an SMV description of the current design.
4
5     -verbose
6         this will print the recursive walk used to export the modules.
7
8     -tpl <template_file>
9         use the given template file. the line containing only the token '%%'
10        is replaced with the regular output of this command.
11

```

12 THIS COMMAND IS UNDER CONSTRUCTION

### C.218 write\_spice – write design to SPICE netlist file

```

1  write_spice [options] [filename]
2
3  Write the current design to an SPICE netlist file.
4
5  -big_endian
6      generate multi-bit ports in MSB first order
7      (default is LSB first)
8
9  -neg net_name
10     set the net name for constant 0 (default: Vss)
11
12  -pos net_name
13     set the net name for constant 1 (default: Vdd)
14
15  -nc_prefix
16     prefix for not-connected nets (default: _NC)
17
18  -inames
19     include names of internal ($-prefixed) nets in outputs
20     (default is to use net numbers instead)
21
22  -top top_module
23     set the specified module as design top module

```

### C.219 write\_table – write design as connectivity table

```

1  write_table [options] [filename]
2
3  Write the current design as connectivity table. The output is a tab-separated
4  ASCII table with the following columns:
5
6  module name
7  cell name
8  cell type
9  cell port
10 direction
11 signal
12
13 module inputs and outputs are output using cell type and port '-' and with
14 'pi' (primary input) or 'po' (primary output) or 'pio' as direction.

```

### C.220 write\_verilog – write design to Verilog file

```

1  write_verilog [options] [filename]
2
3  Write the current design to a Verilog file.
4
5  -norename
6      without this option all internal object names (the ones with a dollar
7      instead of a backslash prefix) are changed to short names in the
8      format '_<number>_'.
9
10 -renameprefix <prefix>
11     insert this prefix in front of auto-generated instance names
12
13 -noattr
14     with this option no attributes are included in the output
15
16 -attr2comment
17     with this option attributes are included as comments in the output
18
19 -noexpr
20     without this option all internal cells are converted to Verilog
21     expressions.
22
23 -siminit
24     add initial statements with hierarchical refs to initialize FFs when
25     in -noexpr mode.
26
27 -nodec
28     32-bit constant values are by default dumped as decimal numbers,
29     not bit pattern. This option deactivates this feature and instead
30     will write out all constants in binary.
31
32 -decimal
33     dump 32-bit constants in decimal and without size and radix
34
35 -nohex
36     constant values that are compatible with hex output are usually
37     dumped as hex values. This option deactivates this feature and
38     instead will write out all constants in binary.
39
40 -nostr
41     Parameters and attributes that are specified as strings in the
42     original input will be output as strings by this back-end. This
43     deactivates this feature and instead will write string constants
44     as binary numbers.
45
46 -extmem
47     instead of initializing memories using assignments to individual
48     elements, use the '$readmemh' function to read initialization data
49     from a file. This data is written to a file named by appending
50     a sequential index to the Verilog filename and replacing the extension
51     with '.mem', e.g. 'write_verilog -extmem foo.v' writes 'foo-1.mem',
52     'foo-2.mem' and so on.
53
54 -defparam

```

```

55     use 'defparam' statements instead of the Verilog-2001 syntax for
56     cell parameters.
57
58     -blackboxes
59         usually modules with the 'blackbox' attribute are ignored. with
60         this option set only the modules with the 'blackbox' attribute
61         are written to the output file.
62
63     -selected
64         only write selected modules. modules must be selected entirely or
65         not at all.
66
67     -v
68         verbose output (print new names of all renamed wires and cells)
69
70 Note that RTLIL processes can't always be mapped directly to Verilog
71 always blocks. This frontend should only be used to export an RTLIL
72 netlist, i.e. after the "proc" pass has been used to convert all
73 processes to logic networks and registers. A warning is generated when
74 this command is called on a design with RTLIL processes.

```

## C.221 write\_xaiger – write design to XAIGER file

```

1     write_xaiger [options] [filename]
2
3 Write the top module (according to the (* top *) attribute or if only one module
4 is currently selected) to an XAIGER file. Any non $_NOT_, $_AND_, $_ABC9_FF_, or non (
5 pseudo-outputs. Whitebox contents will be taken from the '<module-name>$holes'
6 module, if it exists.
7
8     -ascii
9         write ASCII version of AIGER format
10
11     -map <filename>
12         write an extra file with port and box symbols

```

## C.222 xilinx\_dffopt – Xilinx: optimize FF control signal usage

```

1     xilinx_dffopt [options] [selection]
2
3 Converts hardware clock enable and set/reset signals on FFs to emulation
4 using LUTs, if doing so would improve area. Operates on post-techmap Xilinx
5 cells (LUT*, FD*).
6
7     -lut4
8         Assume a LUT4-based device (instead of a LUT6-based device).

```

**C.223 xilinx\_dsp – Xilinx: pack resources into DSPs**

```

1      xilinx_dsp [options] [selection]
2
3  Pack input registers (A2, A1, B2, B1, C, D, AD; with optional enable/reset),
4  pipeline registers (M; with optional enable/reset), output registers (P; with
5  optional enable/reset), pre-adder and/or post-adder into Xilinx DSP resources.
6
7  Multiply-accumulate operations using the post-adder with feedback on the 'C'
8  input will be folded into the DSP. In this scenario only, the 'C' input can be
9  used to override the current accumulation result with a new value, which will
10 be added to the multiplier result to form the next accumulation result.
11
12 Use of the dedicated 'PCOUT' -> 'PCIN' cascade path is detected for 'P' -> 'C'
13 connections (optionally, where 'P' is right-shifted by 17-bits and used as an
14 input to the post-adder -- a pattern common for summing partial products to
15 implement wide multipliers). Limited support also exists for similar cascading
16 for A and B using '[AB]COUT' -> '[AB]CIN'. Currently, cascade chains are limited
17 to a maximum length of 20 cells, corresponding to the smallest Xilinx 7 Series
18 device.
19
20 This pass is a no-op if the scratchpad variable 'xilinx_dsp.multonly' is set
21 to 1.
22
23
24 Experimental feature: addition/subtractions less than 12 or 24 bits with the
25 '(* use_dsp="simd" *)' attribute attached to the output wire or attached to
26 the add/subtract operator will cause those operations to be implemented using
27 the 'SIMD' feature of DSPs.
28
29 Experimental feature: the presence of a '$ge' cell attached to the registered
30 P output implementing the operation "(P >= <power-of-2>)" will be transformed
31 into using the DSP48E1's pattern detector feature for overflow detection.
32
33     -family {xcup|xcu|xc7|xc6v|xc5v|xc4v|xc6s|xc3sda}
34         select the family to target
35     default: xc7

```

**C.224 xilinx\_srl – Xilinx shift register extraction**

```

1      xilinx_srl [options] [selection]
2
3  This pass converts chains of built-in flops (bit-level: $_DFF_[NP]_, $_DFFE_*
4  and word-level: $dff, $dffe) as well as Xilinx flops (FDRE, FDRE_1) into a
5  $__XILINX_SHREG cell. Chains must be of the same cell type, clock, clock polarity,
6  enable, and enable polarity (where relevant).
7  Flops with resets cannot be mapped to Xilinx devices and will not be inferred.
8
9  -minlen N
10     min length of shift register (default = 3)
11
12 -fixed
13     infer fixed-length shift registers.

```



```
13 |  
14 |     -variable  
15 |         infer variable-length shift registers (i.e. fixed-length shifts where  
16 |         each element also fans-out to a $shiftx cell).
```

## C.225 zinit – add inverters so all FF are zero-initialized

```
1 |     zinit [options] [selection]  
2 |  
3 | Add inverters as needed to make all FFs zero-initialized.  
4 |  
5 |     -all  
6 |         also add zero initialization to uninitialized FFs
```

## Appendix D

# RTLIL Text Representation

This appendix documents the text representation of RTLIL in extended Backus-Naur form (EBNF).

The grammar is not meant to represent semantic limitations. That is, the grammar is “permissive”, and later stages of processing perform more rigorous checks.

The grammar is also not meant to represent the exact grammar used in the RTLIL frontend, since that grammar is specific to processing by `lex` and `yacc`, is even more permissive, and is somewhat less understandable than simple EBNF notation.

Finally, note that all statements (rules ending in `-stmt`) terminate in an end-of-line. Because of this, a statement cannot be broken into multiple lines.

### D.1 Lexical elements

#### D.1.1 Characters

An RTLIL file is a stream of bytes. Strictly speaking, a “character” in an RTLIL file is a single byte. The lexer treats multi-byte encoded characters as consecutive single-byte characters. While other encodings *may* work, UTF-8 is known to be safe to use. Byte order marks at the beginning of the file will cause an error.

ASCII spaces (32) and tabs (9) separate lexer tokens.

A `nonws` character, used in identifiers, is any character whose encoding consists solely of bytes above ASCII space (32).

An `eo1` is one or more consecutive ASCII newlines (10) and carriage returns (13).

#### D.1.2 Identifiers

There are two types of identifiers in RTLIL:

- Publically visible identifiers
- Auto-generated identifiers

---

$\langle id \rangle ::= \langle public-id \rangle \mid \langle autogen-id \rangle$

$\langle public-id \rangle ::= \backslash \langle nonws \rangle +$

$\langle autogen-id \rangle ::= \$ \langle nonws \rangle +$

---

### D.1.3 Values

A *value* consists of a width in bits and a bit representation, most significant bit first. Bits may be any of:

- 0: A logic zero value
- 1: A logic one value
- x: An unknown logic value (or don't care in case patterns)
- z: A high-impedance value (or don't care in case patterns)
- m: A marked bit (internal use only)
- -: A don't care value

An *integer* is simply a signed integer value in decimal format. **Warning:** Integer constants are limited to 32 bits. That is, they may only be in the range  $[-2147483648, 2147483648]$ . Integers outside this range will result in an error.

---

$\langle \text{value} \rangle ::= \langle \text{decimal-digit} \rangle + ' \langle \text{binary-digit} \rangle *$

$\langle \text{decimal-digit} \rangle ::= 0 \mid 1 \mid 2 \mid 3 \mid 4 \mid 5 \mid 6 \mid 7 \mid 8 \mid 9$

$\langle \text{binary-digit} \rangle ::= 0 \mid 1 \mid x \mid z \mid m \mid -$

$\langle \text{integer} \rangle ::= -? \langle \text{decimal-digit} \rangle +$

---

### D.1.4 Strings

A string is a series of characters delimited by double-quote characters. Within a string, any character except ASCII NUL (0) may be used. In addition, certain escapes can be used:

- `\n`: A newline
- `\t`: A tab
- `\ooo`: A character specified as a one, two, or three digit octal value

All other characters may be escaped by a backslash, and become the following character. Thus:

- `\\`: A backslash
- `\"`: A double-quote
- `\r`: An 'r' character

### D.1.5 Comments

A comment starts with a `#` character and proceeds to the end of the line. All comments are ignored.

## D.2 File

A file consists of an optional autoindex statement followed by zero or more modules.

---

```
<file> ::= <autoidx-stmt>? <module>*
```

---

### D.2.1 Autoindex statements

The autoindex statement sets the global autoindex value used by Yosys when it needs to generate a unique name, e.g. \$flatten\$N. The N part is filled with the value of the global autoindex value, which is subsequently incremented. This global has to be dumped into RTLIL, otherwise e.g. dumping and running a pass would have different properties than just running a pass on a warm design.

---

```
<autoidx-stmt> ::= autoidx <integer> <eol>
```

---

### D.2.2 Modules

Declares a module, with zero or more attributes, consisting of zero or more wires, memories, cells, processes, and connections.

---

```
<module> ::= <attr-stmt>* <module-stmt> <module-body> <module-end-stmt>

<module-stmt> ::= module <id> <eol>

<module-body> ::= (<param-stmt>
| <wire>
| <memory>
| <cell>
| <process>
| <conn-stmt>)*

<param-stmt> ::= parameter <id> <constant>? <eol>

<constant> ::= <value> | <integer> | <string>

<module-end-stmt> ::= end <eol>
```

---

### D.2.3 Attribute statements

Declares an attribute with the given identifier and value.

---

```
<attr-stmt> ::= attribute <id> <constant> <eol>
```

---

### D.2.4 Signal specifications

A signal is anything that can be applied to a cell port, i.e. a constant value, all bits or a selection of bits from a wire, or concatenations of those.

**Warning:** When an integer constant is a sigspec, it is always 32 bits wide, 2's complement. For example, a constant of  $-1$  is the same as `32 ' 11111111111111111111111111111111`, while a constant of  $1$  is the same as `32 ' 1`.

See Sec. 4.2.4 for an overview of signal specifications.

---

```

<sigspec> ::= <constant>
           | <wire-id>
           | <sigspec> [ <integer> ( : <integer> )? ]
           | { <sigspec>* }

```

---

### D.2.5 Connections

Declares a connection between the given signals.

---

```

<conn-stmt> ::= connect <sigspec> <sigspec> <eol>

```

---

### D.2.6 Wires

Declares a wire, with zero or more attributes, with the given identifier and options in the enclosing module.

See Sec. 4.2.3 for an overview of wires.

---

```

<wire>      ::= <attr-stmt>* <wire-stmt>

<wire-stmt> ::= wire <wire-option>* <wire-id> <eol>

<wire-id>   ::= <id>

<wire-option> ::= width <integer>
                | offset <integer>
                | input <integer>
                | output <integer>
                | inout <integer>
                | upto
                | signed

```

---

### D.2.7 Memories

Declares a memory, with zero or more attributes, with the given identifier and options in the enclosing module. See Sec. 4.2.6 for an overview of memory cells, and Sec. 5.1.5 for details about memory cell types.

---

```

<memory>      ::= <attr-stmt>* <memory-stmt>
<memory-stmt> ::= memory <memory-option>* <id> <eol>
<memory-option> ::= width <integer>
                  | size <integer>
                  | offset <integer>

```

---

### D.2.8 Cells

Declares a cell, with zero or more attributes, with the given identifier and type in the enclosing module. Cells perform functions on input signals. See Chap. 5 for a detailed list of cell types.

---

```

<cell>        ::= <attr-stmt>* <cell-stmt> <cell-body-stmt>* <cell-end-stmt>
<cell-stmt>   ::= cell <cell-id> <cell-type> <eol>
<cell-id>     ::= <id>
<cell-type>   ::= <id>
<cell-body-stmt> ::= parameter (signed | real)? <id> <constant> <eol>
                  | connect <id> <sigspec> <eol>
<cell-end-stmt> ::= end <eol>

```

---

### D.2.9 Processes

Declares a process, with zero or more attributes, with the given identifier in the enclosing module. The body of a process consists of zero or more assignments, exactly one switch, and zero or more syncs.

See Sec. 4.2.5 for an overview of processes.

---

```

<process>     ::= <attr-stmt>* <proc-stmt> <process-body> <proc-end-stmt>
<proc-stmt>   ::= process <id> <eol>
<process-body> ::= <assign-stmt>* <switch>? <assign-stmt>* <sync>*
<assign-stmt> ::= assign <dest-sigspec> <src-sigspec> <eol>
<dest-sigspec> ::= <sigspec>
<src-sigspec>  ::= <sigspec>
<proc-end-stmt> ::= end <eol>

```

---

### D.2.10 Switches

Switches test a signal for equality against a list of cases. Each case specifies a comma-separated list of signals to check against. If there are no signals in the list, then the case is the default case. The body of a case consists of zero or more switches and assignments. Both switches and cases may have zero or more attributes.

---

```

<switch>          ::= <switch-stmt> <case>* <switch-end-stmt>
<switch-stmt>     := <attr-stmt>* switch <sigspec> <eol>
<case>            ::= <attr-stmt>* <case-stmt> <case-body>
<case-stmt>       ::= case <compare>? <eol>
<compare>         ::= <sigspec> (, <sigspec>)*
<case-body>       ::= (<switch> | <assign-stmt>)*
<switch-end-stmt> ::= end <eol>

```

---

### D.2.11 Syncs

Syncs update signals with other signals when an event happens. Such an event may be:

- An edge or level on a signal
- Global clock ticks
- Initialization
- Always

---

```

<sync>            ::= <sync-stmt> <update-stmt>*
<sync-stmt>       ::= sync <sync-type> <sigspec> <eol>
                   | sync global <eol>
                   | sync init <eol>
                   | sync always <eol>
<sync-type>       ::= low | high | posedge | negedge | edge
<update-stmt>     ::= update <dest-sigspec> <src-sigspec> <eol>

```

---

## Appendix E

# Application Notes

This appendix contains copies of the Yosys application notes.

- Yosys AppNote 010: Converting Verilog to BLIF ..... Page **233**
- Yosys AppNote 011: Interactive Design Investigation ..... Page **236**
- Yosys AppNote 012: Converting Verilog to BTOR ..... Page **245**



## Yosys Application Note 010: Converting Verilog to BLIF

Clifford Wolf  
November 2013

**Abstract**—Verilog-2005 is a powerful Hardware Description Language (HDL) that can be used to easily create complex designs from small HDL code. It is the preferred method of design entry for many designers<sup>1</sup>.

The Berkeley Logic Interchange Format (BLIF) [6] is a simple file format for exchanging sequential logic between programs. It is easy to generate and easy to parse and is therefore the preferred method of design entry for many authors of logic synthesis tools.

Yosys [1] is a feature-rich Open-Source Verilog synthesis tool that can be used to bridge the gap between the two file formats. It implements most of Verilog-2005 and thus can be used to import modern behavioral Verilog designs into BLIF-based design flows without dependencies on proprietary synthesis tools.

The scope of Yosys goes of course far beyond Verilog logic synthesis. But it is a useful and important feature and this Application Note will focus on this aspect of Yosys.

### I. INSTALLATION

Yosys written in C++ (using features from C++11) and is tested on modern Linux. It should compile fine on most UNIX systems with a C++11 compiler. The README file contains useful information on building Yosys and its prerequisites.

Yosys is a large and feature-rich program with a couple of dependencies. It is, however, possible to deactivate some of the dependencies in the Makefile, resulting in features in Yosys becoming unavailable. When problems with building Yosys are encountered, a user who is only interested in the features of Yosys that are discussed in this Application Note may deactivate TCL, Qt and MiniSAT support in the Makefile and may opt against building yosys-abc.

This Application Note is based on GIT Rev. e216e0e from 2013-11-23 of Yosys [1]. The Verilog sources used for the examples are taken from yosys-bigsim [2], a collection of real-world designs used for regression testing Yosys.

### II. GETTING STARTED

We start our tour with the Navré processor from yosys-bigsim. The Navré processor [3] is an Open Source AVR clone. It is a single module (softusb\_navre) in a single design file (softusb\_navre.v). It also is using only features that map nicely to the BLIF format, for example it only uses synchronous resets.

Converting softusb\_navre.v to softusb\_navre.blif could not be easier:

```
1 | yosys -o softusb_navre.blif -S softusb_navre.v
```

Listing 1. Calling Yosys without script file

Behind the scenes Yosys is controlled by synthesis scripts that execute commands that operate on Yosys' internal state. For example, the -o softusb\_navre.blif option just adds the command write\_blif softusb\_navre.blif to the end of the script. Likewise a file on the command line - softusb\_navre.v

<sup>1</sup>The other half prefers VHDL, a very different but – of course – equally powerful language.

in this case – adds the command read\_verilog softusb\_navre.v to the beginning of the synthesis script. In both cases the file type is detected from the file extension.

Finally the option -S instantiates a built-in default synthesis script. Instead of using -S one could also specify the synthesis commands for the script on the command line using the -p option, either using individual options for each command or by passing one big command string with a semicolon-separated list of commands. But in most cases it is more convenient to use an actual script file.

### III. USING A SYNTHESIS SCRIPT

With a script file we have better control over Yosys. The following script file replicates what the command from the last section did:

```
1 | read_verilog softusb_navre.v
2 | hierarchy
3 | proc; opt; memory; opt; techmap; opt
4 | write_blif softusb_navre.blif
```

Listing 2. softusb\_navre.js

The first and last line obviously read the Verilog file and write the BLIF file.

The 2nd line checks the design hierarchy and instantiates parametrized versions of the modules in the design, if necessary. In the case of this simple design this is a no-op. However, as a general rule a synthesis script should always contain this command as first command after reading the input files.

The 3rd line does most of the actual work:

- The command `opt` is the Yosys' built-in optimizer. It can perform some simple optimizations such as const-folding and removing unconnected parts of the design. It is common practice to call `opt` after each major step in the synthesis procedure. In cases where too much optimization is not appreciated (for example when analyzing a design), it is recommended to call `clean` instead of `opt`.
- The command `proc` converts *processes* (Yosys' internal representation of Verilog `always-` and `initial-` blocks) to circuits of multiplexers and storage elements (various types of flip-flops).
- The command `memory` converts Yosys' internal representations of arrays and array accesses to multi-port block memories, and then maps this block memories to address decoders and flip-flops, unless the option `-nomap` is used, in which case the multi-port block memories stay in the design and can then be mapped to architecture-specific memory primitives using other commands.
- The command `techmap` turns a high-level circuit with coarse grain cells such as wide adders and multipliers to a fine-grain circuit of simple logic primitives and single-bit storage elements. The command does that by substituting the complex cells by circuits of simpler cells. It is possible to provide a custom set of rules for this process in the form of a Verilog source file, as we will see in the next section.

Now Yosys can be run with the filename of the synthesis script as argument:

```
1 | yosys softusb_navre.js
```

Listing 3. Calling Yosys with script file

Now that we are using a synthesis script we can easily modify how Yosys synthesizes the design. The first thing we should customize is the call to the `hierarchy` command:

Whenever it is known that there are no implicit blackboxes in the design, i.e. modules that are referenced but are not defined, the `hierarchy` command should be called with the `-check` option. This will then cause synthesis to fail when implicit blackboxes are found in the design.

The 2nd thing we can improve regarding the `hierarchy` command is that we can tell it the name of the top level module of the design hierarchy. It will then automatically remove all modules that are not referenced from this top level module.

For many designs it is also desired to optimize the encodings for the finite state machines (FSMs) in the design. The `fsm` command finds FSMs, extracts them, performs some basic optimizations and then generate a circuit from the extracted and optimized description. It would also be possible to tell the `fsm` command to leave the FSMs in their extracted form, so they can be further processed using custom commands. But in this case we don't want that.

So now we have the final synthesis script for generating a BLIF file for the Navré CPU:

```
1 read_verilog softusb_navre.v
2 hierarchy -check -top softusb_navre
3 proc; opt; memory; opt; fsm; opt; techmap;
4 write_blif softusb_navre.blif
```

Listing 4. `softusb_navre.ys` (improved)

#### IV. ADVANCED EXAMPLE: THE AMBER23 ARMv2A CPU

Our 2nd example is the Amber23 [4] ARMv2a CPU. Once again we base our example on the Verilog code that is included in `yosys-bigsim` [2].

The problem with this core is that it contains no dedicated reset logic. Instead the coding techniques shown in Listing 6 are used to define reset values for the global asynchronous reset in an FPGA

```
1 read_verilog a23_alu.v
2 read_verilog a23_barrel_shift_fpga.v
3 read_verilog a23_barrel_shift.v
4 read_verilog a23_cache.v
5 read_verilog a23_coprocessor.v
6 read_verilog a23_core.v
7 read_verilog a23_decode.v
8 read_verilog a23_execute.v
9 read_verilog a23_fetch.v
10 read_verilog a23_multiply.v
11 read_verilog a23_ram_register_bank.v
12 read_verilog a23_register_bank.v
13 read_verilog a23_wishbone.v
14 read_verilog generic_sram_byte_en.v
15 read_verilog generic_sram_line_en.v
16 hierarchy -check -top a23_core
17 add -global_input globrst 1
18 proc -global_arst globrst
19 techmap -map adff2dff.v
20 opt; memory; opt; fsm; opt; techmap
21 write_blif amber23.blif
```

Listing 5. `amber23.ys`

```
1 reg [7:0] a = 13, b;
2 initial b = 37;
```

Listing 6. Implicit coding of global asynchronous resets

implementation. This design can not be expressed in BLIF as it is. Instead we need to use a synthesis script that transforms this form to synchronous resets that can be expressed in BLIF.

(Note that there is no problem if this coding techniques are used to model ROM, where the register is initialized using this syntax but is never updated otherwise.)

Listing 5 shows the synthesis script for the Amber23 core. In line 17 the `add` command is used to add a 1-bit wide global input signal with the name `globrst`. That means that an input with that name is added to each module in the design hierarchy and then all module instantiations are altered so that this new signal is connected throughout the whole design hierarchy.

In line 18 the `proc` command is called. But in this script the signal name `globrst` is passed to the command as a global reset signal for resetting the registers to their assigned initial values.

Finally in line 19 the `techmap` command is used to replace all instances of flip-flops with asynchronous resets with flip-flops with synchronous resets. The map file used for this is shown in Listing 7. Note how the `techmap_celltype` attribute is used in line 1 to tell the `techmap` command which cells to replace in the design, how the `_TECHMAP_FAIL_` wire in lines 15 and 16 (which evaluates to a constant value) determines if the parameter set is compatible with this replacement circuit, and how the `_TECHMAP_DO_` wire in line 13 provides a mini synthesis-script to be used to process this cell.

```
1 (* techmap_celltype = "$adff" *)
2 module adff2dff (CLK, ARST, D, Q);
3
4 parameter WIDTH = 1;
5 parameter CLK_POLARITY = 1;
6 parameter ARST_POLARITY = 1;
7 parameter ARST_VALUE = 0;
8
9 input CLK, ARST;
10 input [WIDTH-1:0] D;
11 output reg [WIDTH-1:0] Q;
12
13 wire [1023:0] _TECHMAP_DO_ = "proc";
14
15 wire _TECHMAP_FAIL_ =
16     !CLK_POLARITY || !ARST_POLARITY;
17
18 always @(posedge CLK)
19     if (ARST)
20         Q <= ARST_VALUE;
21     else
22         Q <= D;
23
24 endmodule
```

Listing 7. `adff2dff.v`

```

1  #include <stdint.h>
2  #include <stdbool.h>
3
4  #define BITMAP_SIZE 64
5  #define OUTPUT 0x10000000
6
7  static uint32_t bitmap[BITMAP_SIZE/32];
8
9  static void bitmap_set(uint32_t idx) { bitmap[idx/32] |= 1 << (idx % 32); }
10 static bool bitmap_get(uint32_t idx) { return (bitmap[idx/32] & (1 << (idx % 32))) != 0; }
11 static void output(uint32_t val) { *((volatile uint32_t*)OUTPUT) = val; }
12
13 int main() {
14     uint32_t i, j, k;
15     output(2);
16     for (i = 0; i < BITMAP_SIZE; i++) {
17         if (bitmap_get(i)) continue;
18         output(3+2*i);
19         for (j = 2*(3+2*i); j += 3+2*i) {
20             if (j%2 == 0) continue;
21             k = (j-3)/2;
22             if (k >= BITMAP_SIZE) break;
23             bitmap_set(k);
24         }
25     }
26     output(0);
27     return 0;
28 }

```

Listing 8. Test program for the Amber23 CPU (Sieve of Eratosthenes). Compiled using GCC 4.6.3 for ARM with `-Os -marm -march=armv2a -mno-thumb-interwork -ffreestanding`, linked with `--fix-v4bx` set and booted with a custom setup routine written in ARM assembler.

## V. VERIFICATION OF THE AMBER23 CPU

The BLIF file for the Amber23 core, generated using Listings 5 and 7 and the version of the Amber23 RTL source that is bundled with yosys-bigsim, was verified using the test-bench from yosys-bigsim. It successfully executed the program shown in Listing 8 in the test-bench.

For simulation the BLIF file was converted back to Verilog using ABC [5]. So this test includes the successful transformation of the BLIF file into ABC’s internal format as well.

The only thing left to write about the simulation itself is that it probably was one of the most energy inefficient and time consuming ways of successfully calculating the first 31 primes the author has ever conducted.

## VI. LIMITATIONS

At the time of this writing Yosys does not support multi-dimensional memories, does not support writing to individual bits of array elements, does not support initialization of arrays with `$readmemb` and `$readmemh`, and has only limited support for tristate logic, to name just a few limitations.

That being said, Yosys can synthesize an overwhelming majority of real-world Verilog RTL code. The remaining cases can usually be modified to be compatible with Yosys quite easily.

The various designs in yosys-bigsim are a good place to look for examples of what is within the capabilities of Yosys.

## VII. CONCLUSION

Yosys is a feature-rich Verilog-2005 synthesis tool. It has many uses, but one is to provide an easy gateway from high-level Verilog code to low-level logic circuits.

The command line option `-S` can be used to quickly synthesize Verilog code to BLIF files without a hassle.

With custom synthesis scripts it becomes possible to easily perform high-level optimizations, such as re-encoding FSMs. In some extreme cases, such as the Amber23 ARMv2 CPU, the more advanced Yosys features can be used to change a design to fit a certain need without actually touching the RTL code.

## REFERENCES

- [1] Clifford Wolf. The Yosys Open Synthesis Suite.  
<http://www.clifford.at/yosys/>
- [2] yosys-bigsim, a collection of real-world Verilog designs for regression testing purposes.  
<https://github.com/cliffordwolf/yosys-bigsim>
- [3] Sebastien Bourdeauducq. Navré AVR clone (8-bit RISC).  
<http://opencores.org/project,navre>
- [4] Conor Santifort. Amber ARM-compatible core.  
<http://opencores.org/project,amber>
- [5] Berkeley Logic Synthesis and Verification Group. ABC: A System for Sequential Synthesis and Verification.  
<http://www.eecs.berkeley.edu/~alanmi/abc/>
- [6] Berkeley Logic Interchange Format (BLIF)  
<http://vlsi.colorado.edu/~vis/blif.ps>

## Yosys Application Note 011: Interactive Design Investigation

Clifford Wolf

Original Version December 2013

**Abstract**—Yosys [1] can be a great environment for building custom synthesis flows. It can also be an excellent tool for teaching and learning Verilog based RTL synthesis. In both applications it is of great importance to be able to analyze the designs it produces easily.

This Yosys application note covers the generation of circuit diagrams with the Yosys show command, the selection of interesting parts of the circuit using the select command, and briefly discusses advanced investigation commands for evaluating circuits and solving SAT problems.

### I. INSTALLATION AND PREREQUISITES

This Application Note is based on the Yosys [1] GIT Rev. 2b90ba1 from 2013-12-08. The README file covers how to install Yosys. The show command requires a working installation of GraphViz [2] and [3] for generating the actual circuit diagrams.

### II. OVERVIEW

This application note is structured as follows:

Sec. III introduces the show command and explains the symbols used in the circuit diagrams generated by it.

Sec. IV introduces additional commands used to navigate in the design, select portions of the design, and print additional information on the elements in the design that are not contained in the circuit diagrams.

Sec. V introduces commands to evaluate the design and solve SAT problems within the design.

Sec. VI concludes the document and summarizes the key points.

### III. INTRODUCTION TO THE SHOW COMMAND

The show command generates a circuit diagram for the design in its current state. Various options can be used to change the appearance of the circuit diagram, set the name and format for the output file, and so forth. When called without any special options, it saves the circuit diagram in a temporary file and launches xdot to display the diagram. Subsequent calls to show re-use the xdot instance (if still running).

```

1 $ cat example.ys
2 read_verilog example.v
3 show -pause
4 proc
5 show -pause
6 opt
7 show -pause
8
9 $ cat example.v
10 module example(input clk, a, b, c,
11                output reg [1:0] y);
12     always @(posedge clk)
13         if (c)
14             y <= c ? a + b : 2'd0;
15 endmodule

```

Figure 1. Yosys script with show commands and example design

#### A. A simple circuit

Fig. 1 shows a simple synthesis script and a Verilog file that demonstrate the usage of show in a simple setting. Note that show is called with the -pause option, that halts execution of the Yosys script until the user presses the Enter key. The show -pause command also allows the user to enter an interactive shell to further investigate the circuit before continuing synthesis.

So this script, when executed, will show the design after each of the three synthesis commands. The generated circuit diagrams are shown in Fig. 2.

The first diagram (from top to bottom) shows the design directly after being read by the Verilog front-end. Input and output ports are displayed as octagonal shapes. Cells are displayed as rectangles with inputs on the left and outputs on the right side. The cell labels are two lines long: The first line contains a unique identifier for the cell and the second line contains the cell type. Internal cell types are prefixed with a dollar sign. The Yosys manual contains a chapter on the internal cell library used in Yosys.

Constants are shown as ellipses with the constant value as label. The syntax <bit\_width>'<bits> is used for constants that are not 32-bit wide and/or contain bits that are not 0 or 1 (i.e. x or z). Ordinary 32-bit constants are written using decimal numbers.

Single-bit signals are shown as thin arrows pointing from the driver to the load. Signals that are multiple bits wide are shown as thick arrows.

Finally *processes* are shown in boxes with round corners. Processes are Yosys' internal representation of the decision-trees and synchronization events modelled in a Verilog always-block. The label reads PROC followed by a unique identifier in the first line and contains the source code location of the original always-block in the 2nd line. Note how the multiplexer from the ?:-expression is represented as a \$mux cell but the multiplexer from the if-statement is yet still hidden within the process.

The proc command transforms the process from the first diagram into a multiplexer and a d-type flip-flop, which brings us to the 2nd diagram.

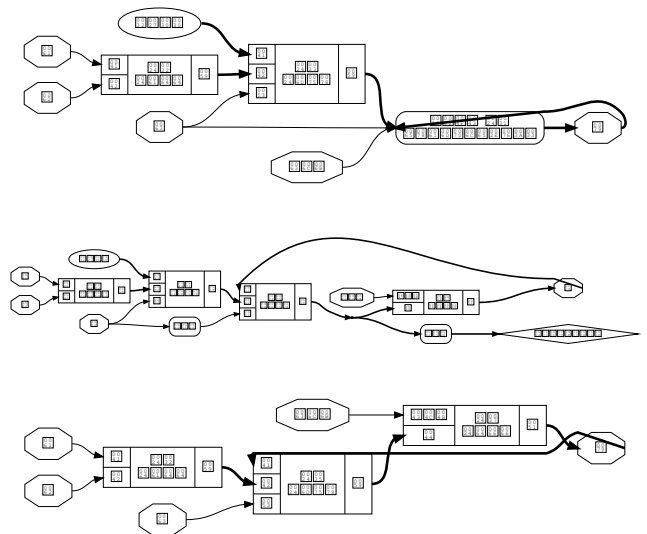


Figure 2. Output of the three show commands from Fig. 1

The Rhombus shape to the right is a dangling wire. (Wire nodes are only shown if they are dangling or have “public” names, for example names assigned from the Verilog input.) Also note that the design now contains two instances of a BUF-node. This is artefacts left behind by the `proc`-command. It is quite usual to see such artefacts after calling commands that perform changes in the design, as most commands only care about doing the transformation in the least complicated way, not about cleaning up after them. The next call to `clean` (or `opt`, which includes `clean` as one of its operations) will clean up this artefacts. This operation is so common in Yosys scripts that it can simply be abbreviated with the `;;` token, which doubles as separator for commands. Unless one wants to specifically analyze this artefacts left behind some operations, it is therefore recommended to always call `clean` before calling `show`.

In this script we directly call `opt` as next step, which finally leads us to the 3rd diagram in Fig. 2. Here we see that the `opt` command not only has removed the artifacts left behind by `proc`, but also determined correctly that it can remove the first \$mux cell without changing the behavior of the circuit.

### B. Break-out boxes for signal vectors

As has been indicated by the last example, Yosys is can manage signal vectors (aka. multi-bit wires or buses) as native objects. This provides great advantages when analyzing circuits that operate on wide integers. But it also introduces some additional complexity when the individual bits of a signal vector are accessed. The example show in Fig. 3 and 4 demonstrates how such circuits are visualized by the `show` command.

The key elements in understanding this circuit diagram are of course the boxes with round corners and rows labeled `<MSB_LEFT>: <LSB_LEFT>` – `<MSB_RIGHT>: <LSB_RIGHT>`. Each of this boxes has one signal per row on one side and a common signal for all rows on the other side. The `<MSB>: <LSB>` tuples specify which bits

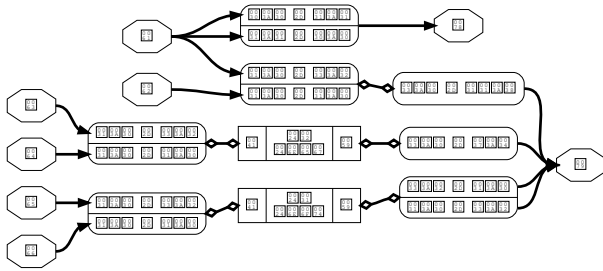


Figure 3. Output of `yosys -p 'proc; opt; show' splice.v`

```

1 module splice_demo(a, b, c, d, e, f, x, y);
2
3   input [1:0] a, b, c, d, e, f;
4   output [1:0] x = {a[0], a[1]};
5
6   output [11:0] y;
7   assign {y[11:4], y[1:0], y[3:2]} =
8         {a, b, ~{c, d}, ~{e, f}};
9
10  endmodule

```

Figure 4. `splice.v`

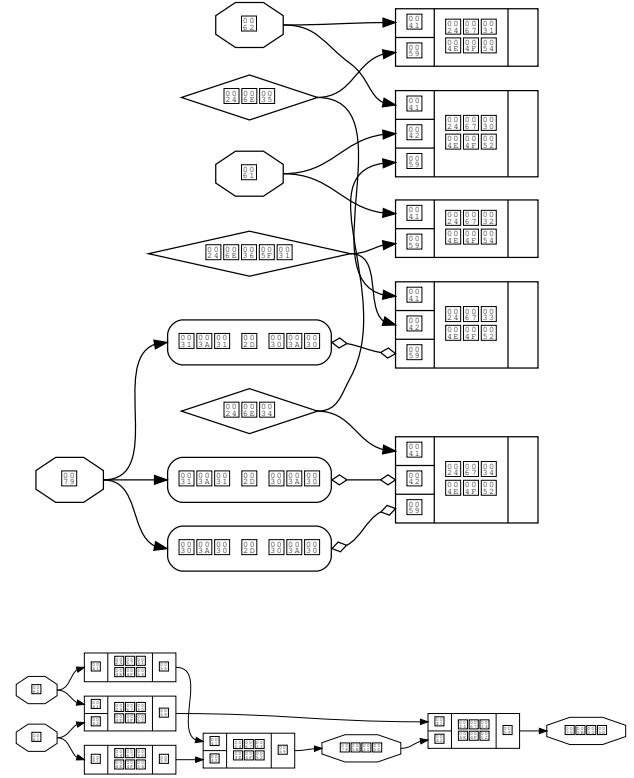


Figure 5. Effects of `splitnets` command and of providing a cell library. (The circuit is a half-adder built from simple CMOS gates.)

of the signals are broken out and connected. So the top row of the box connecting the signals `a` and `x` indicates that the bit 0 (i.e. the range 0:0) from signal `a` is connected to bit 1 (i.e. the range 1:1) of signal `x`.

Lines connecting such boxes together and lines connecting such boxes to cell ports have a slightly different look to emphasise that they are not actual signal wires but a necessity of the graphical representation. This distinction seems like a technicality, until one wants to debug a problem related to the way Yosys internally represents signal vectors, for example when writing custom Yosys commands.

### C. Gate level netlists

Finally Fig. 5 shows two common pitfalls when working with designs mapped to a cell library. The top figure has two problems: First Yosys did not have access to the cell library when this diagram was generated, resulting in all cell ports defaulting to being inputs. This is why all ports are drawn on the left side the cells are awkwardly arranged in a large column. Secondly the two-bit vector `y` requires breakout-boxes for its individual bits, resulting in an unnecessary complex diagram.

For the 2nd diagram Yosys has been given a description of the cell library as Verilog file containing blackbox modules. There are two ways to load cell descriptions into Yosys: First the Verilog file for the cell library can be passed directly to the `show` command using the `-lib <filename>` option. Secondly it is possible to load cell libraries into the design with the `read_verilog -lib <filename>` command. The 2nd method has the great advantage

that the library only needs to be loaded once and can then be used in all subsequent calls to the `show` command.

In addition to that, the 2nd diagram was generated after `split-net -ports` was run on the design. This command splits all signal vectors into individual signal bits, which is often desirable when looking at gate-level circuits. The `-ports` option is required to also split module ports. Per default the command only operates on interior signals.

#### D. Miscellaneous notes

Per default the `show` command outputs a temporary dot file and launches `xdot` to display it. The options `-format`, `-viewer` and `-prefix` can be used to change format, viewer and filename prefix. Note that the `pdf` and `ps` format are the only formats that support plotting multiple modules in one run.

In densely connected circuits it is sometimes hard to keep track of the individual signal wires. For this cases it can be useful to call `show` with the `-colors <integer>` argument, which randomly assigns colors to the nets. The integer ( $> 0$ ) is used as seed value for the random color assignments. Sometimes it is necessary it try some values to find an assignment of colors that looks good.

The command `help show` prints a complete listing of all options supported by the `show` command.

### IV. NAVIGATING THE DESIGN

Plotting circuit diagrams for entire modules in the design brings us only helps in simple cases. For complex modules the generated circuit diagrams are just stupidly big and are no help at all. In such cases one first has to select the relevant portions of the circuit.

In addition to *what* to display one also needs to carefully decide *when* to display it, with respect to the synthesis flow. In general it is a good idea to troubleshoot a circuit in the earliest state in which a problem can be reproduced. So if, for example, the internal state before calling the `techmap` command already fails to verify, it is better to troubleshoot the coarse-grain version of the circuit before `techmap` than the gate-level circuit after `techmap`.

Note: It is generally recommended to verify the internal state of a design by writing it to a Verilog file using `write_verilog -noexpr` and using the simulation models from `simlib.v` and `simcells.v` from the Yosys data directory (as printed by `yosys-config --datdir`).

#### A. Interactive Navigation

Once the right state within the synthesis flow for debugging the circuit has been identified, it is recommended to simply add the `shell` command to the matching place in the synthesis script. This command will stop the synthesis at the specified moment and go to shell mode, where the user can interactively enter commands.

For most cases, the shell will start with the whole design selected (i.e. when the synthesis script does not already narrow the selection). The command `ls` can now be used to create a list of all modules. The command `cd` can be used to switch to one of the modules (type `cd ..` to switch back). Now the `ls` command lists the objects within that module. Fig. 6 demonstrates this using the design from Fig. 1.

There is a thing to note in Fig. 6: We can see that the cell names from Fig. 2 are just abbreviations of the actual cell names, namely the part after the last dollar-sign. Most auto-generated names (the ones starting with a dollar sign) are rather long and contains some additional information on the origin of the named object. But in most cases those names can simply be abbreviated using the last part.

```

1 yosys> ls
2
3 1 modules:
4   example
5
6 yosys> cd example
7
8 yosys [example]> ls
9
10 7 wires:
11   $0\y[1:0]
12   $add$example.v:5$2_Y
13   a
14   b
15   c
16   clk
17   y
18
19 3 cells:
20   $add$example.v:5$2
21   $procdf$7
22   $procmux$5

```

Figure 6. Demonstration of `ls` and `cd` using `example.v` from Fig. 1

Usually all interactive work is done with one module selected using the `cd` command. But it is also possible to work from the design-context (`cd ..`). In this case all object names must be prefixed with `<module_name>/. For example a*/b* would refer to all objects whose names start with b from all modules whose names start with a.`

The `dump` command can be used to print all information about an object. For example `dump $2` will print Fig. 7. This can for example be useful to determine the names of nets connected to cells, as the net-names are usually suppressed in the circuit diagram if they are auto-generated.

For the remainder of this document we will assume that the commands are run from module-context and not design-context.

#### B. Working with selections

When a module is selected using the `cd` command, all commands (with a few exceptions, such as the `read_*` and `write_*` commands) operate only on the selected module. This can also be useful for synthesis scripts where different synthesis strategies should be applied to different modules in the design.

```

1 attribute \src "example.v:5"
2 cell $add $add$example.v:5$2
3   parameter \A_SIGNED 0
4   parameter \A_WIDTH 1
5   parameter \B_SIGNED 0
6   parameter \B_WIDTH 1
7   parameter \Y_WIDTH 2
8   connect \A \a
9   connect \B \b
10   connect \Y $add$example.v:5$2_Y
11 end

```

Figure 7. Output of `dump $2` using the design from Fig. 1 and Fig. 2

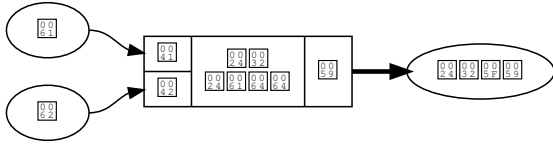


Figure 8. Output of show after select \$2 or select t:\$add (see also Fig. 2)

But for most interactive work we want to further narrow the set of selected objects. This can be done using the select command.

For example, if the command select \$2 is executed, a subsequent show command will yield the diagram shown in Fig. 8. Note that the nets are now displayed in ellipses. This indicates that they are not selected, but only shown because the diagram contains a cell that is connected to the net. This of course makes no difference for the circuit that is shown, but it can be a useful information when manipulating selections.

Objects can not only be selected by their name but also by other properties. For example select t:\$add will select all cells of type \$add. In this case this also yields the diagram shown in Fig. 8.

The output of help select contains a complete syntax reference for matching different properties.

Many commands can operate on explicit selections. For example the command dump t:\$add will print information on all \$add cells in the active module. Whenever a command has [selection] as last argument in its usage help, this means that it will use the engine behind the select command to evaluate additional arguments and use the resulting selection instead of the selection created by the last select command.

Normally the select command overwrites a previous selection. The commands select -add and select -del can be used to add or remove objects from the current selection.

The command select -clear can be used to reset the selection to the default, which is a complete selection of everything in the current module.

### C. Operations on selections

The select command is actually much more powerful than it might seem on the first glimpse. When it is called with multiple arguments, each argument is evaluated and pushed separately on a stack. After all arguments have been processed it simply creates the union of all elements on the stack. So the following command will select all \$add cells and all objects with the foo attribute set:

```

1 module foobaraddsub(a, b, c, d, fa, fs, ba, bs);
2   input [7:0] a, b, c, d;
3   output [7:0] fa, fs, ba, bs;
4   assign fa = a + (* foo *) b;
5   assign fs = a - (* foo *) b;
6   assign ba = c + (* bar *) d;
7   assign bs = c - (* bar *) d;
8 endmodule

```

Figure 9. Test module for operations on selections

```

1 module sumprod(a, b, c, sum, prod);
2
3   input [7:0] a, b, c;
4   output [7:0] sum, prod;
5
6   {* sumstuff *}
7   assign sum = a + b + c;
8   {* *}
9
10  assign prod = a * b * c;
11
12 endmodule

```

Figure 10. Another test module for operations on selections

select t:\$add a:foo

(Try this with the design shown in Fig. 9. Use the select -list command to list the current selection.)

In many cases simply adding more and more stuff to the selection is an ineffective way of selecting the interesting part of the design. Special arguments can be used to combine the elements on the stack. For example the %i argument pops the last two elements from the stack, intersects them, and pushes the result back on the stack. So the following command will select all \$add cells that have the foo attribute set:

select t:\$add a:foo %i

The listing in Fig. 10 uses the Yosys non-standard { \* ... \* } syntax to set the attribute sumstuff on all cells generated by the first assign statement. (This works on arbitrary large blocks of Verilog code and can be used to mark portions of code for analysis.)

Selecting a:sumstuff in this module will yield the circuit diagram shown in Fig. 11. As only the cells themselves are selected, but not the temporary wire \$1\_Y, the two adders are shown as two disjunct parts. This can be very useful for global signals like clock and reset signals: just unselect them using a command such as select -del clk rst and each cell using them will get its own net label.

In this case however we would like to see the cells connected properly. This can be achieved using the %X action, that broadens the selection, i.e. for each selected wire it selects all cells connected to the wire and vice versa. So show a:sumstuff %X yields the diagram shown in Fig. 12.

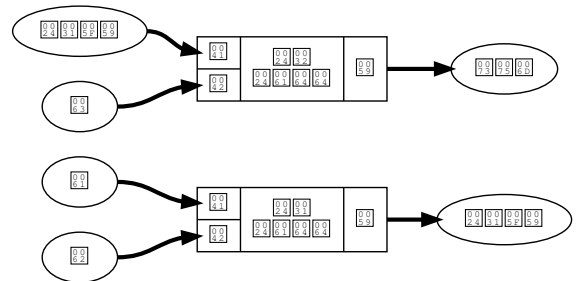


Figure 11. Output of show a:sumstuff on Fig. 10

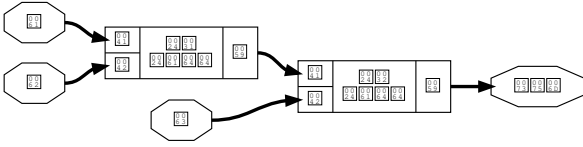


Figure 12. Output of `show a:sumstuff %x` on Fig. 10

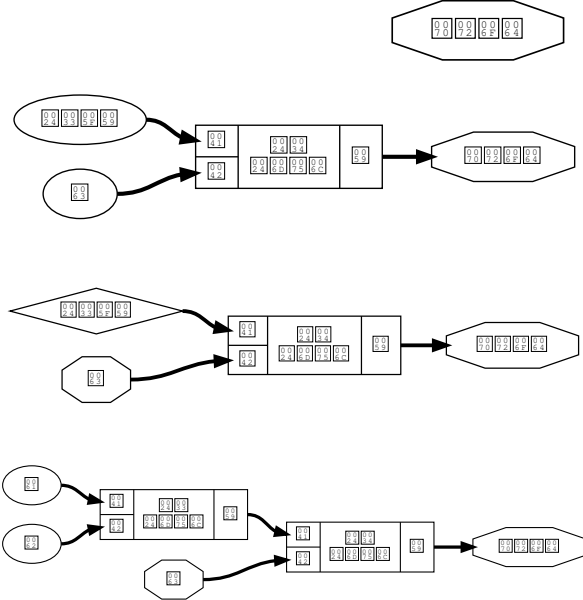


Figure 13. Objects selected by `select prod %ci...`

#### D. Selecting logic cones

Fig. 12 shows what is called the *input cone* of `sum`, i.e. all cells and signals that are used to generate the signal `sum`. The `%ci` action can be used to select the input cones of all object in the top selection in the stack maintained by the `select` command.

As the `%x` action, this commands broadens the selection by one “step”. But this time the operation only works against the direction of data flow. That means, wires only select cells via output ports and cells only select wires via input ports.

Fig. 13 show the sequence of diagrams generated by the following commands:

```
show prod
show prod %ci
show prod %ci %ci
show prod %ci %ci %ci
```

When selecting many levels of logic, repeating `%ci` over and over again can be a bit dull. So there is a shortcut for that: the number of iterations can be appended to the action. So for example the action `%ci3` is identical to performing the `%ci` action three times.

The action `%ci*` performs the `%ci` action over and over again until it has no effect anymore.

In most cases there are certain cell types and/or ports that should not be considered for the `%ci` action, or we only want to follow

certain cell types and/or ports. This can be achieved using additional patterns that can be appended to the `%ci` action.

Lets consider the design from Fig. 14. It serves no purpose other than being a non-trivial circuit for demonstrating some of the advanced Yosys features. We synthesize the circuit using `proc; opt; memory; opt` and change to the `memdemo` module with `cd memdemo`. If we type `show now` we see the diagram shown in Fig. 15.

But maybe we are only interested in the tree of multiplexers that select the output value. In order to get there, we would start by just showing the output signal and its immediate predecessors:

```
show y %ci2
```

From this we would learn that `y` is driven by a `$dff` cell, that `y` is connected to the output port `Q`, that the `clk` signal goes into the `CLK` input port of the cell, and that the data comes from a auto-generated wire into the input `D` of the flip-flop cell.

As we are not interested in the clock signal we add an additional pattern to the `%ci` action, that tells it to only follow ports `Q` and `D` of `$dff` cells:

```
show y %ci2:+$dff[Q,D]
```

To add a pattern we add a colon followed by the pattern to the `%ci` action. The pattern it self starts with `-` or `+`, indicating if it is an include or exclude pattern, followed by an optional comma separated list of cell types, followed by an optional comma separated list of port names in square brackets.

Since we know that the only cell considered in this case is a `$dff` cell, we could as well only specify the port names:

```
show y %ci2:+[Q,D]
```

Or we could decide to tell the `%ci` action to not follow the `CLK` input:

```
show y %ci2:-[CLK]
```

Next we would investigate the next logic level by adding another `%ci2` to the command:

```
show y %ci2:-[CLK] %ci2
```

```
1 module memdemo(clk, d, y);
2
3 input clk;
4 input [3:0] d;
5 output reg [3:0] y;
6
7 integer i;
8 reg [1:0] s1, s2;
9 reg [3:0] mem [0:3];
10
11 always @(posedge clk) begin
12     for (i = 0; i < 4; i = i+1)
13         mem[i] <= mem[(i+1) % 4] + mem[(i+2) % 4];
14     { s2, s1 } = d ? { s1, s2 } ^ d : 4'b0;
15     mem[s1] <= d;
16     y <= mem[s2];
17 end
18
19 endmodule
```

Figure 14. Demo circuit for demonstrating some advanced Yosys features



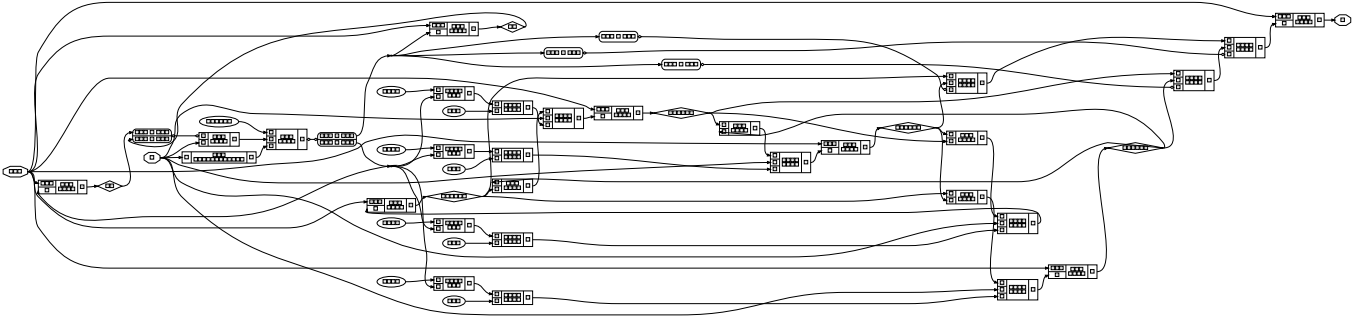


Figure 15. Complete circuit diagram for the design shown in Fig. 14

From this we would learn that the next cell is a \$mux cell and we would add additional pattern to narrow the selection on the path we are interested. In the end we would end up with a command such as

```
show y %ci2:+$dff[Q,D] %ci*:-$mux[S]:-$dff
```

in which the first %ci jumps over the initial d-type flip-flop and the 2nd action selects the entire input cone without going over multiplexer select inputs and flip-flop cells. The diagram produced by this command is shown in Fig. 16.

Similar to %ci exists an action %co to select output cones that accepts the same syntax for pattern and repetition. The %x action mentioned previously also accepts this advanced syntax.

This actions for traversing the circuit graph, combined with the actions for boolean operations such as intersection (%i) and difference (%d) are powerful tools for extracting the relevant portions of the circuit under investigation.

See help select for a complete list of actions available in selections.

#### E. Storing and recalling selections

The current selection can be stored in memory with the command `select -set <name>`. It can later be recalled using `select @<name>`. In fact, the @<name> expression pushes the stored selection on the stack maintained by the select command. So for example

```
select @foo @bar %i
```

will select the intersection between the stored selections foo and bar.

In larger investigation efforts it is highly recommended to maintain a script that sets up relevant selections, so they can easily be

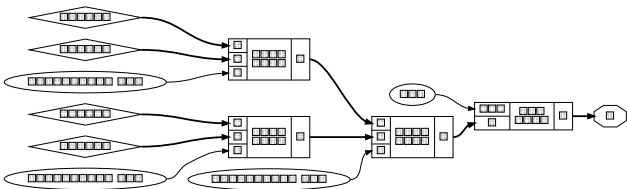


Figure 16. Output of `show y %ci2:+$dff[Q,D] %ci*:-$mux[S]:-$dff`

recalled, for example when Yosys needs to be re-run after a design or source code change.

The history command can be used to list all recent interactive commands. This feature can be useful for creating such a script from the commands used in an interactive session.

#### V. ADVANCED INVESTIGATION TECHNIQUES

When working with very large modules, it is often not enough to just select the interesting part of the module. Instead it can be useful to extract the interesting part of the circuit into a separate module. This can for example be useful if one wants to run a series of synthesis commands on the critical part of the module and wants to carefully read all the debug output created by the commands in order to spot a problem. This kind of troubleshooting is much easier if the circuit under investigation is encapsulated in a separate module.

Fig. 17 shows how the submod command can be used to split the circuit from Fig. 14 and 15 into its components. The -name option is used to specify the name of the new module and also the name of the new cell in the current module.

##### A. Evaluation of combinatorial circuits

The eval command can be used to evaluate combinatorial circuits. For example (see Fig. 17 for the circuit diagram of selstage):

```
yosys [selstage]> eval -set s2,s1 4'b1001 -set d 4'hc -show n2 -show
```

9. Executing EVAL pass (evaluate the circuit given an input).

Full command line: eval -set s2,s1 4'b1001 -set d 4'hc -show n2 -show

Eval result: \n2 = 2'10.

Eval result: \n1 = 2'10.

So the -set option is used to set input values and the -show option is used to specify the nets to evaluate. If no -show option is specified, all selected output ports are used per default.

If a necessary input value is not given, an error is produced. The option -set-undef can be used to instead set all unspecified input nets to undef (x).

The -table option can be used to create a truth table. For example:

```
yosys [selstage]> eval -set-undef -set d[3:1] 0 -table s1,d[0]
```

10. Executing EVAL pass (evaluate the circuit given an input).

Full command line: eval -set-undef -set d[3:1] 0 -table s1,d[0]

\s1	\d [0]	\n1	\n2
2'00	1'0	2'00	2'00
2'00	1'1	2'xx	2'00
2'01	1'0	2'00	2'00

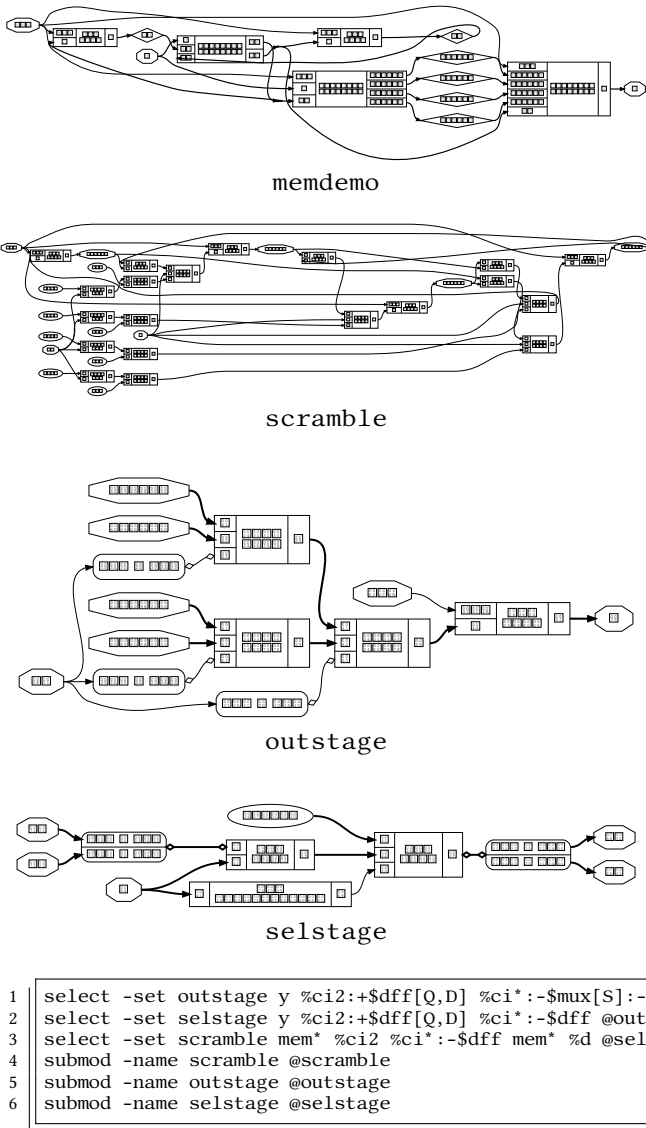


Figure 17. The circuit from Fig. 14 and 15 broken up using submod

```

2'01  1'1 | 2'xx 2'01
2'10  1'0 | 2'00 2'00
2'10  1'1 | 2'xx 2'10
2'11  1'0 | 2'00 2'00
2'11  1'1 | 2'xx 2'11

```

Assumed undef (x) value for the following signals: \s2

Note that the `eval` command (as well as the `sat` command discussed in the next sections) does only operate on flattened modules. It can not analyze signals that are passed through design hierarchy levels. So the `flatten` command must be used on modules that instantiate other modules before this commands can be applied.

### B. Solving combinatorial SAT problems

Often the opposite of the `eval` command is needed, i.e. the circuits output is given and we want to find the matching input signals. For small circuits with only a few input bits this can be accomplished by trying all possible input combinations, as it is done by the `eval -table` command. For larger circuits however, Yosys

provides the `sat` command that uses a SAT [4] solver [5] to solve this kind of problems.

The `sat` command works very similar to the `eval` command. The main difference is that it is now also possible to set output values and find the corresponding input values. For Example:

```
yosys [selstage]> sat -show s1,s2,d -set s1 s2 -set n2,n1 4'b1001
```

11. Executing SAT pass (solving SAT problems in the circuit).  
Full command line: `sat -show s1,s2,d -set s1 s2 -set n2,n1 4'b1001`

```

Setting up SAT problem:
Import set-constraint: \s1 = \s2
Import set-constraint: { \n2 \n1 } = 4'b1001
Final constraint equation: { \n2 \n1 \s1 } = { 4'b1001 \s2 }
Imported 3 cells to SAT database.
Import show expression: { \s1 \s2 \d }

```

Solving problem with 81 variables and 207 clauses..  
SAT solving finished - model found:

Signal Name	Dec	Hex	Bin
\d	9	9	1001
\s1	0	0	00
\s2	0	0	00

Note that the `sat` command supports signal names in both arguments to the `-set` option. In the above example we used `-set s1 s2` to constraint `s1` and `s2` to be equal. When more complex constraints are needed, a wrapper circuit must be constructed that checks the constraints and signals if the constraint was met using an extra output port, which then can be forced to a value using the `-set` option. (Such a circuit that contains the circuit under test plus additional constraint checking circuitry is called a *miter* circuit.)

Fig. 18 shows a miter circuit that is supposed to be used as a prime number test. If `ok` is 1 for all input values `a` and `b` for a given `p`, then `p` is prime, or at least that is the idea.

The Yosys shell session shown in Fig. 19 demonstrates that SAT solvers can even find the unexpected solutions to a problem: Using integer overflow there actually is a way of “factorizing” 31. The clean solution would of course be to perform the test in 32 bits, for example by replacing `p != a*b` in the miter with `p != {16'd0,a}*b`, or by using a temporary variable for the 32 bit product `a*b`. But as 31 fits well into 8 bits (and as the purpose of this document is to show off Yosys features) we can also simply force the upper 8 bits of `a` and `b` to zero for the `sat` call, as is done in the second command in Fig. 19 (line 31).

The `-prove` option used in this example works similar to `-set`, but tries to find a case in which the two arguments are not equal. If such a case is not found, the property is proven to hold for all inputs that satisfy the other constraints.

It might be worth noting, that SAT solvers are not particularly efficient at factorizing large numbers. But if a small factorization problem occurs as part of a larger circuit problem, the Yosys SAT solver is perfectly capable of solving it.

```

1 module primetest(p, a, b, ok);
2   input [15:0] p, a, b;
3   output ok = p != a*b || a == 1 || b == 1;
4   endmodule

```

Figure 18. A simple miter circuit for testing if a number is prime. But it has a problem (see main text and Fig. 19).

```

1 yosys [primetest]> sat -prove ok 1 -set p 31
2
3 8. Executing SAT pass (solving SAT problems in the circuit).
4 Full command line: sat -prove ok 1 -set p 31
5
6 Setting up SAT problem:
7 Import set-constraint: \p = 16'0000000000011111
8 Final constraint equation: \p = 16'0000000000011111
9 Imported 6 cells to SAT database.
10 Import proof-constraint: \ok = 1'1
11 Final proof equation: \ok = 1'1
12
13 Solving problem with 2790 variables and 8241 clauses..
14 SAT proof finished - model found: FAIL!
15
16
17 (-----\
18 -----) )-----\
19 |-----/-----\ /----- (-----) (-----|
20 |-----|-----|-----|-----|-----|-----|
21 |-----|-----|-----|-----|-----|-----|
22
23
24 Signal Name          Dec          Hex          Bin
25 -----
26 \a                   15029       3ab5       0011101010110101
27 \b                   4099        1003       0001000000000011
28 \ok                   0           0           0
29 \p                   31           1f          0000000000011111
30
31 yosys [primetest]> sat -prove ok 1 -set p 31 -set a[15:8],b[15:8] 0
32
33 9. Executing SAT pass (solving SAT problems in the circuit).
34 Full command line: sat -prove ok 1 -set p 31 -set a[15:8],b[15:8] 0
35
36 Setting up SAT problem:
37 Import set-constraint: \p = 16'0000000000011111
38 Import set-constraint: { \a [15:8] \b [15:8] } = 16'0000000000000000
39 Final constraint equation: { \a [15:8] \b [15:8] \p } = { 16'0000000000000000 16'0000000000011111 }
40 Imported 6 cells to SAT database.
41 Import proof-constraint: \ok = 1'1
42 Final proof equation: \ok = 1'1
43
44 Solving problem with 2790 variables and 8257 clauses..
45 SAT proof finished - no model found: SUCCESS!
46
47
48 /$$$$$$ /$$$$$$ /$$$$$$
49 /$$_ $$ /$$_ $$ /$$_ $$
50 | $$ \ $$ | $$ \ $$ | $$ \ $$
51 | $$ | $$ | $$ | $$ | $$ | $$
52 | $$ | $$ | $$ | $$ | $$ | $$
53 | $$$/ $$ $$$/ $$ $$$/ $$
54 | $$$$$$ /$$ $$$$$$ /$$ $$$$$$ /$$
55 |_____ $$$|_____/|_____/|_____/|_____/

```

Figure 19. Experiments with the miter circuit from Fig. 18. The first attempt of proving that 31 is prime failed because the SAT solver found a creative way of factorizing 31 using integer overflow.

### C. Solving sequential SAT problems

The SAT solver functionality in Yosys can not only be used to solve combinatorial problems, but can also solve sequential problems. Let's consider the entire memdemo module from Fig. 14 and suppose we want to know which sequence of input values for d will cause the output y to produce the sequence 1, 2, 3 from any initial state. Fig. 20 show the solution to this question, as produced

by the following command:

```
sat -seq 6 -show y -show d -set-init-undef \
-max_undef -set-at 4 y 1 -set-at 5 y 2 -set-at 6 y 3
```

The -seq 6 option instructs the sat command to solve a sequential problem in 6 time steps. (Experiments with lower number of steps have show that at least 3 cycles are necessary to bring the circuit in a state from which the sequence 1, 2, 3 can be produced.)

The `-set-init-undef` option tells the `sat` command to initialize all registers to the `undef (x)` state. The way the `x` state is treated in Verilog will ensure that the solution will work for any initial state.

The `-max_undef` option instructs the `sat` command to find a solution with a maximum number of undefs. This way we can see clearly which inputs bits are relevant to the solution.

Finally the three `-set-at` options add constraints for the `y` signal to play the 1, 2, 3 sequence, starting with time step 4.

It is not surprising that the solution sets `d = 0` in the first step, as this is the only way of setting the `s1` and `s2` registers to a known value. The input values for the other steps are a bit harder to work out manually, but the SAT solver finds the correct solution in an instant.

There is much more to write about the `sat` command. For example, there is a set of options that can be used to perform sequential proofs using temporal induction [6]. The command `help sat` can be used to print a list of all options with short descriptions of their functions.

## VI. CONCLUSION

Yosys provides a wide range of functions to analyze and investigate designs. For many cases it is sufficient to simply display circuit diagrams, maybe use some additional commands to narrow the scope of the circuit diagrams to the interesting parts of the circuit. But some cases require more than that. For this applications Yosys provides commands that can be used to further inspect the behavior of the circuit, either by evaluating which output values are generated from certain input values (`eval`) or by evaluation which input values and initial conditions can result in a certain behavior at the outputs (`sat`). The SAT command can even be used to prove (or disprove) theorems regarding the circuit, in more advanced cases with the additional help of a miter circuit.

This features can be powerful tools for the circuit designer using Yosys as a utility for building circuits and the software developer using Yosys as a framework for new algorithms alike.

## REFERENCES

- [1] Clifford Wolf. The Yosys Open SYnthesis Suite. <http://www.clifford.at/yosys/>
- [2] Graphviz - Graph Visualization Software. <http://www.graphviz.org/>
- [3] xdot.py - an interactive viewer for graphs written in Graphviz's dot language. <https://github.com/jrfonseca/xdot.py>
- [4] *Circuit satisfiability problem* on Wikipedia [http://en.wikipedia.org/wiki/Circuit\\_satisfiability](http://en.wikipedia.org/wiki/Circuit_satisfiability)
- [5] MiniSat: a minimalistic open-source SAT solver. <http://minisat.se/>
- [6] Niklas Een and Niklas Sörensson (2003). Temporal Induction by Incremental SAT Solving. <http://citeseerx.ist.psu.edu/viewdoc/summary?doi=10.1.1.4.8161>

```

1  yosys [memdemo]> sat -seq 6 -show y -show d -set-init-undef \
2  -max_undef -set-at 4 y 1 -set-at 5 y 2 -set-at 6 y 3
3
4  6. Executing SAT pass (solving SAT problems in the circuit).
5  Full command line: sat -seq 6 -show y -show d -set-init-undef
6  -max_undef -set-at 4 y 1 -set-at 5 y 2 -set-at 6 y 3
7
8  Setting up time step 1:
9  Final constraint equation: { } = { }
10 Imported 29 cells to SAT database.
11
12 Setting up time step 2:
13 Final constraint equation: { } = { }
14 Imported 29 cells to SAT database.
15
16 Setting up time step 3:
17 Final constraint equation: { } = { }
18 Imported 29 cells to SAT database.
19
20 Setting up time step 4:
21 Import set-constraint for timestep: \y = 4'0001
22 Final constraint equation: \y = 4'0001
23 Imported 29 cells to SAT database.
24
25 Setting up time step 5:
26 Import set-constraint for timestep: \y = 4'0010
27 Final constraint equation: \y = 4'0010
28 Imported 29 cells to SAT database.
29
30 Setting up time step 6:
31 Import set-constraint for timestep: \y = 4'0011
32 Final constraint equation: \y = 4'0011
33 Imported 29 cells to SAT database.
34
35 Setting up initial state:
36 Final constraint equation: { \y \s2 \s1 \mem[3] \mem[2] \mem[1]
37 \mem[0] } = 24'xxxxxxxxxxxxxxxxxxxxxxxxxxxx
38
39 Import show expression: \y
40 Import show expression: \d
41
42 Solving problem with 10322 variables and 27881 clauses..
43 SAT model found. maximizing number of undefs.
44 SAT solving finished - model found:
45
46
47   Time Signal Name      Dec
48   Hex||      Bin
49   --||-----
50   init \mem[0]      --
51   --||      xxxx
52   init \mem[1]      --
53   --||      xxxx
54   init \mem[2]      --
55   --||      xxxx
56   init \mem[3]      --
57   --||      xxxx
58   init \s1          --
59   --||      xx
60   init \s2          --
61   --||      xx
62   init \y           --
63   --||      xxxx
64   -----
65   0 1 \d            0
66   --||      0000
67   1 1 \y            --
68   --||      xxxx
69   -----
70   2 2 \d            1
71   --||      0001
72   1 2 \y            --
73   --||      xxxx
74   -----
75   3 3 \d            2
76   --||      0010
77   0 3 \y            0
78   --||      0000
79   -----
80   4 4 \d            3
81   --||      0011
82   1 4 \y            1
83   --||      0001
84   -----
85   5 5 \d            --
86   --||      001x
87   2 5 \y            2
88   --||      0010
89   -----
90   6 6 \d            --
91   --||      xxxx
92   3 6 \y            3
93   --||      0011

```

Figure 20. Solving a sequential SAT problem in the `memdemo` module from Fig. 14.

## Yosys Application Note 012: Converting Verilog to BTOR

Ahmed Irfan and Clifford Wolf  
April 2015

**Abstract**—Verilog-2005 is a powerful Hardware Description Language (HDL) that can be used to easily create complex designs from small HDL code. BTOR [3] is a bit-precise word-level format for model checking. It is a simple format and easy to parse. It allows to model the model checking problem over the theory of bit-vectors with one-dimensional arrays, thus enabling to model Verilog designs with registers and memories. Yosys [1] is an Open-Source Verilog synthesis tool that can be used to convert Verilog designs with simple assertions to BTOR format.

### I. INSTALLATION

Yosys written in C++ (using features from C++11) and is tested on modern Linux. It should compile fine on most UNIX systems with a C++11 compiler. The README file contains useful information on building Yosys and its prerequisites.

Yosys is a large and feature-rich program with some dependencies. For this work, we may deactivate other extra features such as TCL and ABC support in the Makefile.

This Application Note is based on GIT Rev. 082550f from 2015-04-04 of Yosys [1].

### II. QUICK START

We assume that the Verilog design is synthesizable and we also assume that the design does not have multi-dimensional memories. As BTOR implicitly initializes registers to zero value and memories stay uninitialized, we assume that the Verilog design does not contain initial blocks. For more details about the BTOR format, please refer to [3].

We provide a shell script `verilog2btor.sh` which can be used to convert a Verilog design to BTOR. The script can be found in the `backends/btor` directory. The following example shows its usage:

```
verilog2btor.sh fsm.v fsm.btor test
```

Listing 1. Using verilog2btor script

The script `verilog2btor.sh` takes three parameters. In the above example, the first parameter `fsm.v` is the input design, the second parameter `fsm.btor` is the file name of BTOR output, and the third parameter `test` is the name of top module in the design.

To specify the properties (that need to be checked), we have two options:

- We can use the Verilog `assert` statement in the procedural block or module body of the Verilog design, as shown in Listing 2. This is the preferred option.
- We can use a single-bit output wire, whose name starts with `safety`. The value of this output wire needs to be driven low when the property is met, i.e. the solver will try to find a model that makes the safety pin go high. This is demonstrated in Listing 3.

```
module test(input clk, input rst, output y);

    reg [2:0] state;

    always @(posedge clk) begin
        if (rst || state == 3) begin
            state <= 0;
        end else begin
            assert(state < 3);
            state <= state + 1;
        end
    end

    assign y = state[2];

    assert property (y != 1'b1);

endmodule
```

Listing 2. Specifying property in Verilog design with assert

```
module test(input clk, input rst,
            output y, output safety1);

    reg [2:0] state;

    always @(posedge clk) begin
        if (rst || state == 3)
            state <= 0;
        else
            state <= state + 1;
        end

    assign y = state[2];

    assign safety1 = !(y != 1'b1);

endmodule
```

Listing 3. Specifying property in Verilog design with output wire

We can run Boolector [2] 1.4.1<sup>1</sup> on the generated BTOR file:

```
$ boolector fsm.btor
unsat
```

Listing 4. Running boolector on BTOR file

We can also use nuXmv [4], but on BTOR designs it does not support memories yet. With the next release of nuXmv, we will be also able to verify designs with memories.

### III. DETAILED FLOW

Yosys is able to synthesize Verilog designs up to the gate level. We are interested in keeping registers and memories when synthesizing the design. For this purpose, we describe a customized Yosys synthesis flow, that is also provided by the `verilog2btor.sh`

<sup>1</sup> Newer version of Boolector do not support sequential models. Boolector 1.4.1 can be built with picosat-951. Newer versions of picosat have an incompatible API.

script. Listing 5 shows the Yosys commands that are executed by `verilog2btor.sh`.

```

1 read_verilog -sv $1;
2 hierarchy -top $3; hierarchy -libdir $DIR;
3 hierarchy -check;
4 proc; opt;
5 opt_expr -mux_undef; opt;
6 rename -hide;;;
7 splice; opt;
8 memory_dff -wr_only; memory_collect;;
9 flatten;;
10 memory_unpack;
11 splitnets -driver;
12 setundef -zero -undriven;
13 opt;;;
14 write_btor $2;
```

Listing 5. Synthesis Flow for BTOR with memories

```

read_verilog -sv $1;
hierarchy -top $3; hierarchy -libdir $DIR;
hierarchy -check;
proc; opt;
opt_expr -mux_undef; opt;
rename -hide;;;
splice; opt;
memory;;
flatten;;
splitnets -driver;
setundef -zero -undriven;
opt;;;
write_btor $2;
```

Listing 6. Synthesis Flow for BTOR without memories

Here is short description of what is happening in the script line by line:

- 1) Reading the input file.
- 2) Setting the top module in the hierarchy and trying to read automatically the files which are given as `include` in the file read in first line.
- 3) Checking the design hierarchy.
- 4) Converting processes to multiplexers (muxs) and flip-flops.
- 5) Removing undef signals from muxs.
- 6) Hiding all signal names that are not used as module ports.
- 7) Explicit type conversion, by introducing slice and concat cells in the circuit.
- 8) Converting write memories to synchronous memories, and collecting the memories to multi-port memories.
- 9) Flattening the design to get only one module.
- 10) Separating read and write memories.
- 11) Splitting the signals that are partially assigned
- 12) Setting undef to zero value.
- 13) Final optimization pass.
- 14) Writing BTOR file.

For detailed description of the commands mentioned above, please refer to the Yosys documentation, or run `yosys -h command_name`.

The script presented earlier can be easily modified to have a BTOR file that does not contain memories. This is done by removing the line number 8 and 10, and introduces a new command `memory` at line number 8. Listing 6 shows the modified Yosys script file:

Here is an example Verilog design that we want to convert to BTOR:

```

module array(input clk);

    reg [7:0] counter;
    reg [7:0] mem [7:0];

    always @(posedge clk) begin
        counter <= counter + 8'd1;
        mem[counter] <= counter;
    end

    assert property (!(counter > 8'd0) ||
        mem[counter - 8'd1] == counter - 8'd1);

endmodule
```

Listing 7. Example - Verilog Design

The generated BTOR file that contain memories, using the script shown in Listing 5:

```

1 var 1 clk
2 array 8 3
3 var 8 $auto$rename.cc:150:execute$20
4 const 8 00000001
5 sub 8 3 4
6 slice 3 5 2 0
7 read 8 2 6
8 slice 3 3 2 0
9 add 8 3 4
10 const 8 00000000
11 ugt 1 3 10
12 not 1 11
13 const 8 11111111
14 slice 1 13 0 0
15 one 1
16 eq 1 1 15
17 and 1 16 14
18 write 8 3 2 8 3
19 acond 8 3 17 18 2
20 anext 8 3 2 19
21 eq 1 7 5
22 or 1 12 21
23 const 1 1
24 one 1
25 eq 1 23 24
26 cond 1 25 22 24
27 root 1 -26
28 cond 8 1 9 3
29 next 8 3 28

```

Listing 8. Example - Converted BTOR with memory

```

1 var 1 clk
2 var 8 mem[0]
3 var 8 $auto$rename.cc:150:execute$20
4 slice 3 3 2 0
5 slice 1 4 0 0
6 not 1 5
7 slice 1 4 1 1
8 not 1 7
9 slice 1 4 2 2
10 not 1 9
11 and 1 8 10
12 and 1 6 11
13 cond 8 12 3 2
14 cond 8 1 13 2
15 next 8 2 14
16 const 8 00000001
17 add 8 3 16
18 const 8 00000000
19 ugt 1 3 18
20 not 1 19
21 var 8 mem[2]
22 and 1 7 10
23 and 1 6 22
24 cond 8 23 3 21
25 cond 8 1 24 21
26 next 8 21 25
27 sub 8 3 16
:
54 cond 1 53 50 52
55 root 1 -54
:
77 cond 8 76 3 44
78 cond 8 1 77 44
79 next 8 44 78

```

Listing 9. Example - Converted BTOR without memory

## V. LIMITATIONS

BTOR does not support initialization of memories and registers, i.e. they are implicitly initialized to value zero, so the initial block for memories need to be removed when converting to BTOR. It should also be kept in consideration that BTOR does not support the x or z values of Verilog.

Another thing to bear in mind is that Yosys will convert multi-dimensional memories to one-dimensional memories and address decoders. Therefore out-of-bounds memory accesses can yield unexpected results.

## VI. CONCLUSION

Using the described flow, we can use Yosys to generate word-level verification benchmarks with or without memories from Verilog designs.

## REFERENCES

- [1] Clifford Wolf. The Yosys Open Synthesis Suite.  
<http://www.clifford.at/yosys/>
- [2] Robert Brummayer and Armin Biere, Boolector: An Efficient SMT Solver for Bit-Vectors and Arrays  
<http://fmv.jku.at/boolector/>

And the BTOR file obtained by the script shown in Listing 6, which expands the memory into individual elements:

- [3] Robert Brummayer and Armin Biere and Florian Lonsing, BTOR: Bit-Precise Modelling of Word-Level Problems for Model Checking  
<http://fmv.jku.at/papers/BrummayerBiereLonsing-BPR08.pdf>
- [4] Roberto Cavada and Alessandro Cimatti and Michele Dorigatti and Alberto Griggio and Alessandro Mariotti and Andrea Micheli and Sergio Mover and Marco Roveri and Stefano Tonetta, The nuXmv Symbolic Model Checker  
<https://es-static.fbk.eu/tools/nuxmv/index.php>



# Bibliography

- [ASU86] AHO, Alfred V. ; SETHI, Ravi ; ULLMAN, Jeffrey D.: *Compilers: principles, techniques, and tools*. Boston, MA, USA : Addison-Wesley Longman Publishing Co., Inc., 1986. – ISBN 0–201–10088–6
- [BHSV90] BRAYTON, R.K. ; HACHTEL, G.D. ; SANGIOVANNI-VINCENTELLI, A.L.: Multilevel logic synthesis. In: *Proceedings of the IEEE* 78 (1990), Nr. 2, S. 264–300. <http://dx.doi.org/10.1109/5.52213>. – DOI 10.1109/5.52213. – ISSN 0018–9219
- [CI00] CUMMINGS, Clifford E. ; INC, Sunburst D.: Nonblocking Assignments in Verilog Synthesis, Coding Styles That Kill. In: *SNUG (Synopsys Users Group) 2000 User Papers, section-MC1 (1 st paper, 2000*
- [GW13] GLASER, Johann ; WOLF, Clifford: Methodology and Example-Driven Interconnect Synthesis for Designing Heterogeneous Coarse-Grain Reconfigurable Architectures. In: HAASE, Jan (Hrsg.): *Advances in Models, Methods, and Tools for Complex Chip Design — Selected contributions from FDL'12*. Springer, 2013. – to appear
- [HS96] HACHTEL, G D. ; SOMENZI, F: *Logic Synthesis and Verification Algorithms*. 1996
- [IP-10] IEEE Standard for IP-XACT, Standard Structure for Packaging, Integrating, and Reusing IP within Tools Flows. In: *IEEE Std 1685-2009* (2010), S. C1–360. <http://dx.doi.org/10.1109/IEEESTD.2010.5417309>. – DOI 10.1109/IEEESTD.2010.5417309
- [LHBB85] LEE, Kyu Y. ; HOLLEY, Michael ; BAILEY, Mary ; BRIGHT, Walter: A High-Level Design Language for Programmable Logic Devices. In: *VLSI Design (Manhasset NY: CPM Publications)* (June 1985), S. 50–62
- [STGR10] SHI, Yiqiong ; TING, Chan W. ; GWEE, Bah-Hwee ; REN, Ye: A highly efficient method for extracting FSMs from flattened gate-level netlist. In: *Circuits and Systems (ISCAS), Proceedings of 2010 IEEE International Symposium on*, 2010, S. 2610–2613
- [Ull76] ULLMANN, J. R.: An Algorithm for Subgraph Isomorphism. In: *J. ACM* 23 (1976), Januar, Nr. 1, S. 31–42. <http://dx.doi.org/10.1145/321921.321925>. – DOI 10.1145/321921.321925. – ISSN 0004–5411
- [Ver02] IEEE Standard for Verilog Register Transfer Level Synthesis. In: *IEEE Std 1364.1-2002* (2002). <http://dx.doi.org/10.1109/IEEESTD.2002.94220>. – DOI 10.1109/IEEESTD.2002.94220
- [Ver06] IEEE Standard for Verilog Hardware Description Language. In: *IEEE Std 1364-2005 (Revision of IEEE Std 1364-2001)* (2006). <http://dx.doi.org/10.1109/IEEESTD.2006.99495>. – DOI 10.1109/IEEESTD.2006.99495
- [VHD04] IEEE Standard for VHDL Register Transfer Level (RTL) Synthesis. In: *IEEE Std 1076.6-2004 (Revision of IEEE Std 1076.6-1999)* (2004). <http://dx.doi.org/10.1109/IEEESTD.2004.94802>. – DOI 10.1109/IEEESTD.2004.94802
- [VHD09] IEEE Standard VHDL Language Reference Manual. In: *IEEE Std 1076-2008 (Revision of IEEE Std 1076-2002)* (2009), 26. <http://dx.doi.org/10.1109/IEEESTD.2009.4772740>. – DOI 10.1109/IEEESTD.2009.4772740

## BIBLIOGRAPHY

- [WGS<sup>+</sup>12] WOLF, Clifford ; GLASER, Johann ; SCHUPFER, Florian ; HAASE, Jan ; GRIMM, Christoph: Example-driven interconnect synthesis for heterogeneous coarse-grain reconfigurable logic. In: *FDL Proceeding of the 2012 Forum on Specification and Design Languages*, 2012, S. 194–201
- [Wol13] WOLF, Clifford: *Design and Implementation of the Yosys Open SYnthesis Suite*. 2013. – Bachelor Thesis, Vienna University of Technology

# Internet References

- [16] C-to-Verilog. <http://www.c-to-verilog.com/>.
- [17] Flex. <http://flex.sourceforge.net/>.
- [18] GNU Bison. <http://www.gnu.org/software/bison/>.
- [19] LegUp. <http://legup.eecg.utoronto.ca/>.
- [20] OpenCores I<sup>2</sup>C Core. <http://opencores.org/project,i2c>.
- [21] OpenCores k68 Core. <http://opencores.org/project,k68>.
- [22] openMSP430 CPU. <http://opencores.org/project,openmsp430>.
- [23] OpenRISC 1200 CPU. [http://opencores.org/or1k/OR1200\\_OpenRISC\\_Processor](http://opencores.org/or1k/OR1200_OpenRISC_Processor).
- [24] Synopsys Formality Equivalence Checking. <http://www.synopsys.com/Tools/Verification/FormalEquivalence/Pages/Formality.aspx>.
- [25] The Liberty Library Modeling Standard. <http://www.opensourceliberty.org/>.
- [26] Armin Biere, Johannes Kepler University Linz, Austria. AIGER. <http://fmv.jku.at/aiger/>.
- [27] Berkeley Logic Synthesis and Verification Group. ABC: A System for Sequential Synthesis and Verification. HQ Rev b5750272659f, 2012-10-28, <http://www.eecs.berkeley.edu/~alanmi/abc/>.
- [28] M. group at Berkeley studies logic synthesis and verification for VLSI design. MVSIS: Logic Synthesis and Verification. Version 3.0, <http://embedded.eecs.berkeley.edu/mvsis/>.
- [29] M. McCutchen. C++ Big Integer Library. <http://mattmcutchen.net/bigint/>.